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THESIS

COMPUTER SIMULATION OF
DIGITAL SIGNAL MODULATION TECHNIQUES IN
SATELLITE COMMUNICATIONS

by

Craig Dean Carlson

September 1985

Thesis Advisor:

James L. Wayman

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of the FFT's was conducted to determine if there is any relationship between the components of the FFT of the different signals. The statistic used to investigate this possible relationship was the F-distribution. The computer simulation was written and conducted in the FORTRAN programming language. A copy of the program, results of the simulation and the statistical analysis conducted are included in the appendices.

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Computer Simulation of
Digital Signal Modulation Techniques in
Satellite Communications

by

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requirements for the degree of

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ABSTRACT

This thesis is a tutorial on digital signal modulation techniques used in satellite communications and includes computer simulations of those digital signal modulation techniques introduced. The purpose of the thesis is to introduce digital signal modulation techniques and through the use of computer simulation, generate statistics which represent the characteristics of the FFT for the respective signal type. Further, an analysis of the statistics of the FFT's was conducted to determine if there is any relationship between the components of the FFT of the different signals. The statistic used to investigate this possible relationship was the F-distribution. The computer simulation was written and conducted in the FORTRAN programming language. A copy of the program, results of the simulations and the statistical analysis conducted are included in the appendices.

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I. INTRODUCTION

A. BACKGROUND

Since the introduction of the sampling theorem and the matched filter, digital communications techniques have developed into a highly proficient discipline. The marriage of this discipline with the rapidly expanding space program has resulted in communication satellites employing a multitude of digital signal modulation techniques. A modulation technique is a method of transmitting the information contained in a message by varying or modulating the characteristics of a carrier waveform. These methods offer a range of advantages and disadvantages depending on the specific characteristics of the modulation technique employed. The applications of the various signal modulation techniques likewise vary. In order to understand this exciting new field it is necessary to look at some of the aspects of satellite communications systems in general. Then an investigation will be made into the general attributes of digital communications and their relationship to the satellite system.

The ability to understand these digital signal modulation techniques is the first step in being able to intercept, identify and demodulate unknown digital signals. These digital signals, transmitted from unknown sources, are believed to display frequency characteristics peculiar to the modulation technique employed in the encoding process. The digital computer offers unique opportunities in simulating these modulation techniques, in signal processing and in decoding of an intercepted signal.

B. SPECIFIC GOALS

It is the specific goal of this thesis to investigate the open literature on the topic of digital signal modulation techniques in satellite communications. This includes a basic understanding of the communications satellite system as well as the specific techniques employed in signal modulation. Additionally, once a basic understanding of these digital signal modulation techniques is achieved, computer code in the FORTRAN programming language will be developed which simulates these modulated signals. The statistics of the time-varying Fast Fourier Transforms (FFT) of these simulated signals will be investigated. The purpose of this analysis will be to lead to follow-on research in the area of signal analysis of intercepted digital signals whereby they can be classified by their FFT as employing a specific digital signal modulation technique.

C. SCOPE OF THE PROJECT

Although an indepth analysis of all the digital signal modulation techniques which will be introduced involves considerable higher level mathematics, it is not within the scope of this project to delve heavily into the mathematics. It would be advantageous, however, for the reader to have had integral and differential calculus and an introduction to statistics. Also a course in electrical engineering may prove helpful but is not essential since in actuality it is the electrical engineering aspects of satellite communications that this tutorial is attempting to present. The computer programming will be accomplished utilizing the techniques of software engineering and top down modular design. Existing blocks of code will be used as modules whenever appropriate and available. Again it is the

ultimate purpose of this project to examine a variety of digital signal modulation techniques and develop computer code that simulates common signals used in satellite communications that have been produced by one of the many digital signal modulation techniques to be investigated.

II. UNDERSTANDING SATELLITE COMMUNICATIONS

A. HISTORY AND APPLICATIONS

Forty years ago, in 1945, Arthur Clarke first envisioned the use of space stations placed in geosynchronous orbit for communicating to different points on the earth [Ref. 1]. Nine years later in 1954, J.R. Pierce of Bell Laboratories performed a system analysis on such a communications system [Ref. 2]. In 1957, the launch of Sputnik demonstrated the feasibility of using a satellite for just such an application. However, by 1961 the only satellite communications technologies which had been demonstrated were the Courier 1B satellite, a short-life active retransmission teletype communications satellite in a 1000 km orbit, and the Echo I balloon in a 1600 km orbit which demonstrated passive reflection of powerful microwave signals from one earth station to another. Active microwave communications demonstrated in Projects Telstar and Relay were years away [Ref. 3]. The first geostationary orbit was achieved by Project Syncom in 1963 [Ref. 4].

In 1964, communication organizations from several countries joined together to form the international organization of INTELSAT (International Telecommunications Satellite Organization). INTELSAT's purpose was to develop a satellite network which would provide truly global communications capabilities. This resulted in the launch in 1965 of the world's first commercial communications satellite, INTELSAT I, also known as "Early Bird". With "Early Bird", telecommunications utilizing satellite relay were established between the United States and Europe. [Ref. 3]

The reliability of these satellite systems has improved dramatically since INTELSAT I in 1965. Reliability of individual links in the system approach 99.99 percent or higher. Total system reliability exceeding 99.9 percent is common [Ref. 5], making satellite communications more reliable than many other modes of communications. In this sense, reliability is a measure of the probability that no failure will occur in a respective channel or in the system during the design life of the satellite.

In order for the operability, capability and reliability of these systems to have developed at this pace, it was necessary for the technologies associated with them to develop as rapidly or even more rapidly than the systems themselves. Engineering sciences and specifically the fields of aerospace and electrical engineering historically have required between 7 and 10 years to take a concept from operational requirement to full scale operation. This was not the case with the concept of communications satellites which has seen four generations of INTELSAT satellites within a decade's time. [Ref. 3]

The "Early Bird" satellite weighed approximately 38 kilograms and possessed limited power and bandwidth capacity enabling it to carry only 240 two-way telephone conversations. Today's communications satellites represent order-of-magnitude improvements in many important operating parameters such as power and bandwidth. Additionally, increased effective radiated power from the techniques of stabilized earth pointing antennas have greatly increased the capacity of later generation communications satellites. INTELSAT V, the current generation of communications satellites, is a three-axis stabilized platform using not only the 6/4 GHz frequency band (6 GHz receive/4 GHz transmit) as in earlier generation satellites but also a 500 MHz bandwidth available in the 14/11 GHz band. The

separation in the receive and transmit frequencies is necessary to prevent interference during simultaneous operation of the receiver and transmitter. Another factor increasing the capacity of present generation satellites is the increase in primary power available in the satellite.

[Ref. 3]

The technologies which have contributed to the evolution of communications satellites come from two primary sources, namely technology from the space program of the 1960's supported by NASA and DoD and communications technology due largely to commercial and private sector contributions.

[Ref. 3]

Electronic devices and components have contributed significantly to the rapid development of satellite systems. These electronic devices range from something which is now considered basic, i.e., the transistor, to devices such as Traveling Wave Tube amplifiers, lightweight antennas and antenna feed systems. There have been major improvements in satellite power sources including more efficient solar cells and high storage capacity/lightweight batteries. Additionally, two significant developments in electrical engineering have made modern day digital signal processing a reality. They are the sampling theorem and the matched filter. [Ref. 3]

Communications satellites of the future are likely to utilize onboard signal processing. Signal processing functions such as signal reshaping, switching and/or multiplexing and compression could soon take place on the satellite due to the reduction in size and weight of the necessary hardware. Operation at over 100 megabits per second are envisioned. Onboard signal processing will greatly reduce the expense and complexity of earth stations thereby making services of a satellite available to a wider range of small and geographically disperse users. [Ref. 3]

Satellite communications hold great promise to provide service to a multitude of users over a wide area. Applications lie not solely in retransmission but also in data collection from that same large geographic area. Military users have definite applications in these areas when warning, intelligence and surveillance systems provide digital inputs to a central source. Although most of the present applications for satellite communications are still provided by the government, commercial applications have seen tremendous increases in the last several years. [Ref. 3]

B. ORBITS AND LIMITATIONS

Satellite orbits are generally categorized as either equatorial (0 degrees inclination), polar (90 degrees inclination) or inclined at some angle other than 0 or 90 degrees relative to the spin axis of the earth as illustrated in Figure 2.1 [Ref. 6]. Each satellite orbit has a characteristic velocity which is dependent on the height of the orbit and the orbit's eccentricity. Eccentricity is a measure of the degree to which the orbit approximates a circle. A circle has eccentricity equal to zero since the focus is located at the center. See equation 2.1 and Figure 2.2.

A communications satellite in elliptical orbit about the earth obeys Kepler's second law of planetary motion. That is, a satellite's constant angular momentum about the earth means that its areal velocity also remains constant. See Figure 2.3. Of particular interest is the satellite velocity at apogee (V_a) and perigee (V_p) given by equations 2.2 and 2.3.

Note that for a circle, $e = 0$ and $R_a = R_p$. Therefore a satellite in circular orbit about the earth has an orbital velocity as given in equation 2.4.

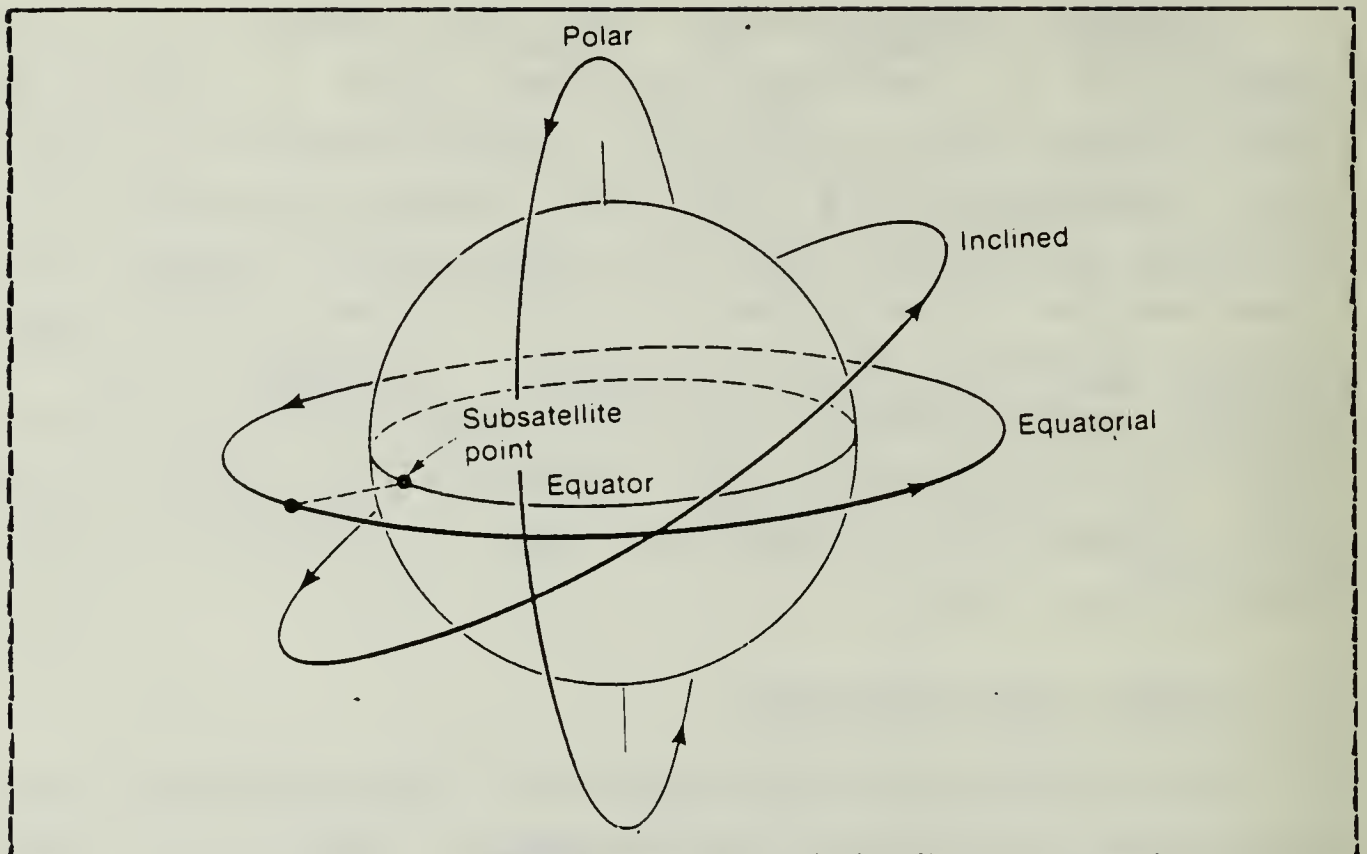


Figure 2.1 Satellite Orbits

Most communications satellites are placed in a circular equatorial orbit where the desire is to stabilize them over a fixed point on the surface of the earth called the subsatellite point. This type of orbit is called geostationary or stationary. Any satellite which has an orbital period equal to the period of rotation of the earth is called synchronous or geosynchronous. These terms are used almost interchangeably in most literature. As mentioned for a geosynchronous communications satellite, the orbital period of the satellite, T , must be equal to the period of rotation of the earth. Kepler's third law of planetary motion can be rewritten to yield equation 2.5.

The period of revolution of the earth for a sidereal day is 23 hr 56 min 4 sec. For that given period there is only one satellite altitude as expressed by Kepler's third law.

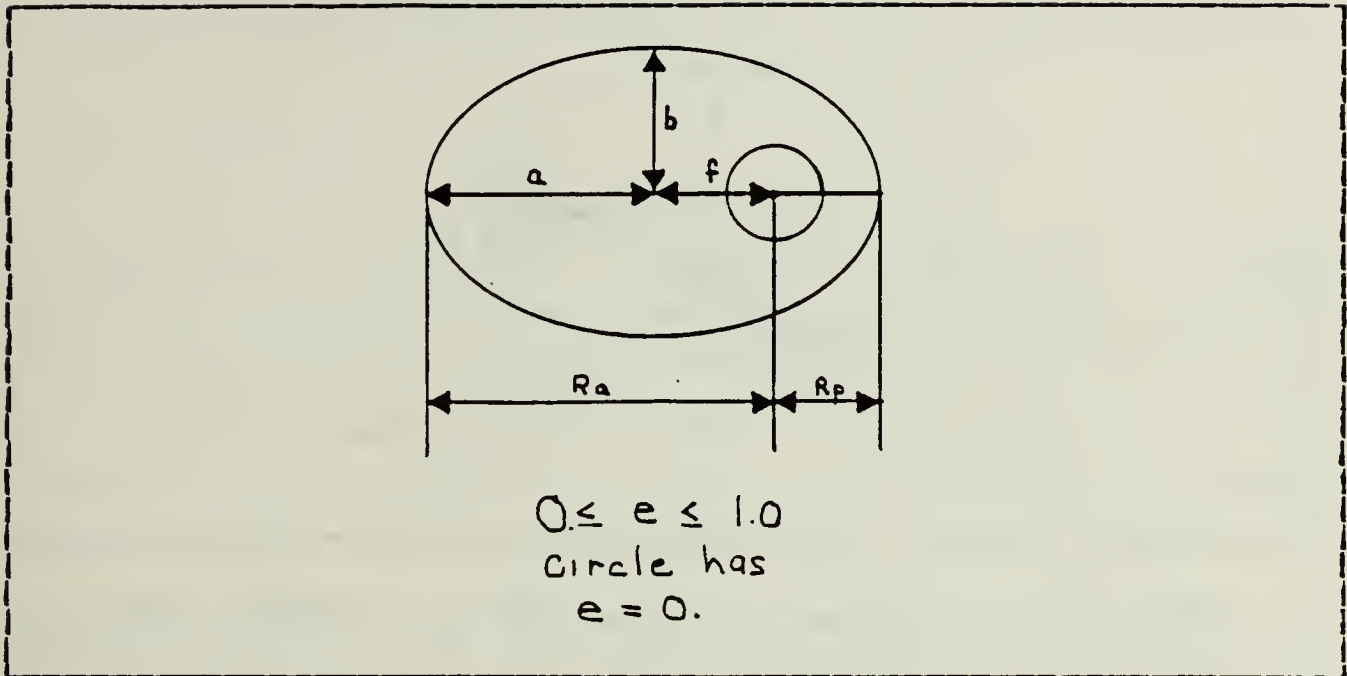


Figure 2.2 Eccentricity

eccentricity (e) = c/a (eqn 2.1)

c = distance from focus

a = semi-major axis

b = semi-minor axis

R_a = radius of apogee

R_p = radius of perigee

By rearranging terms that altitude is given in equation 2.6. Since the orbit is circular, $a = R_a = R_p$ and the height of the orbit above the surface of the earth is $h = a - R_e$; or 35,804 km.

One disadvantage of a geosynchronous communications satellite is the lack of global coverage. These satellites provide excellent coverage of the subsatellite point and

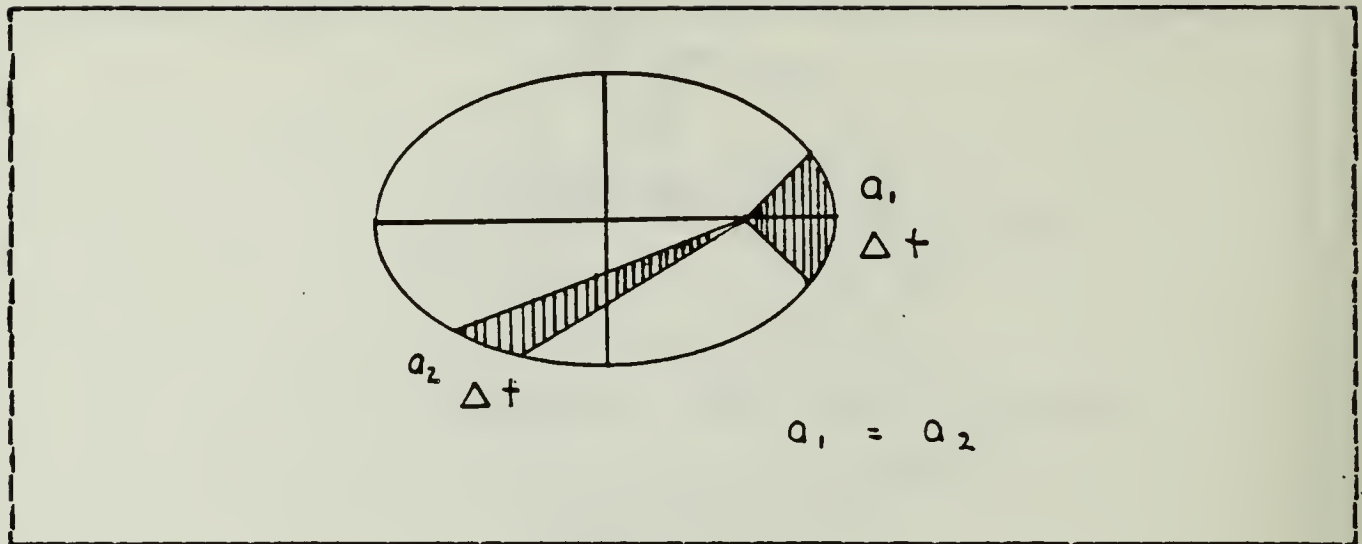


Figure 2.3 Kepler's Second Law of Planetary Motion

$$V_a = (k/R_a(1-e))^{.5} \quad (\text{eqn 2.2})$$

$$V_p = (k/R_p(1+e))^{.5} \quad (\text{eqn 2.3})$$

$$k = G M_e = 3.98866 \times 10^{-11} \text{ m}^3/\text{s}^2$$

G = universal gravitational constant

$$G = 6.67 \times 10^{-11} \text{ N m}^2/\text{kg}^2$$

N = newtons = m kg/s²

$$M_e = \text{mass of the earth} = 5.98 \times 10^{24} \text{ kg}$$

$$V_c = (k/R_c)^{.5} \quad (\text{eqn 2.4})$$

$$R_c = R_e + h$$

$$R_e = \text{radius of the earth} = 6.37 \times 10^6 \text{ m}$$

h = satellite orbital altitude

$$T = 2 \pi a^{1.5} / k^{.5} \quad (\text{eqn 2.5})$$

T = period of rotation

a = semi-major axis

$$a = (T / 2 \pi)^{2/3} (k)^{1/3}$$

(eqn 2.6)

$$a = 42,173 \text{ km}$$

laterally to a latitude of about $\pm 80^\circ$ [Ref. 6]. This is generally no problem for commercial applications since the polar regions do not require a significant degree of access. The military, on the other hand, does have an interest in communications in the polar region and therefore has several communications satellites that have orbits inclined at various angles. This type of orbit generally has disadvantages of lack of continuous coverage and a much more complicated system of ground tracking and receiving stations.

C. FREQUENCY BAND CONSIDERATIONS

Although there appears to be an infinite number of frequencies available for communications, restrictions do exist as to those which are practicable. Limitations on available frequency bands for satellite communications are due to the need to select segments of the electromagnetic spectrum which reduce noise and interference and are most favorable in terms of power efficiency and propagation distortions. Trade offs must be made to arrive at the optimum frequency for a particular application since single frequencies seldom offer the best performance for all variables. The problems arise when consideration is given to the number of users requiring the same frequency bands including terrestrial communications networks. Since the problem of interference is global, a worldwide organization has been established to assign frequency bands for various applications. This organization is called WARC, World Administrative Radio Conference [Ref. 6]. Illustrations of

the portions of the electromagnetic spectrum in question and current allocations of satellite frequency bands are shown in Figures 2.4 and 2.5 [Ref. 6].

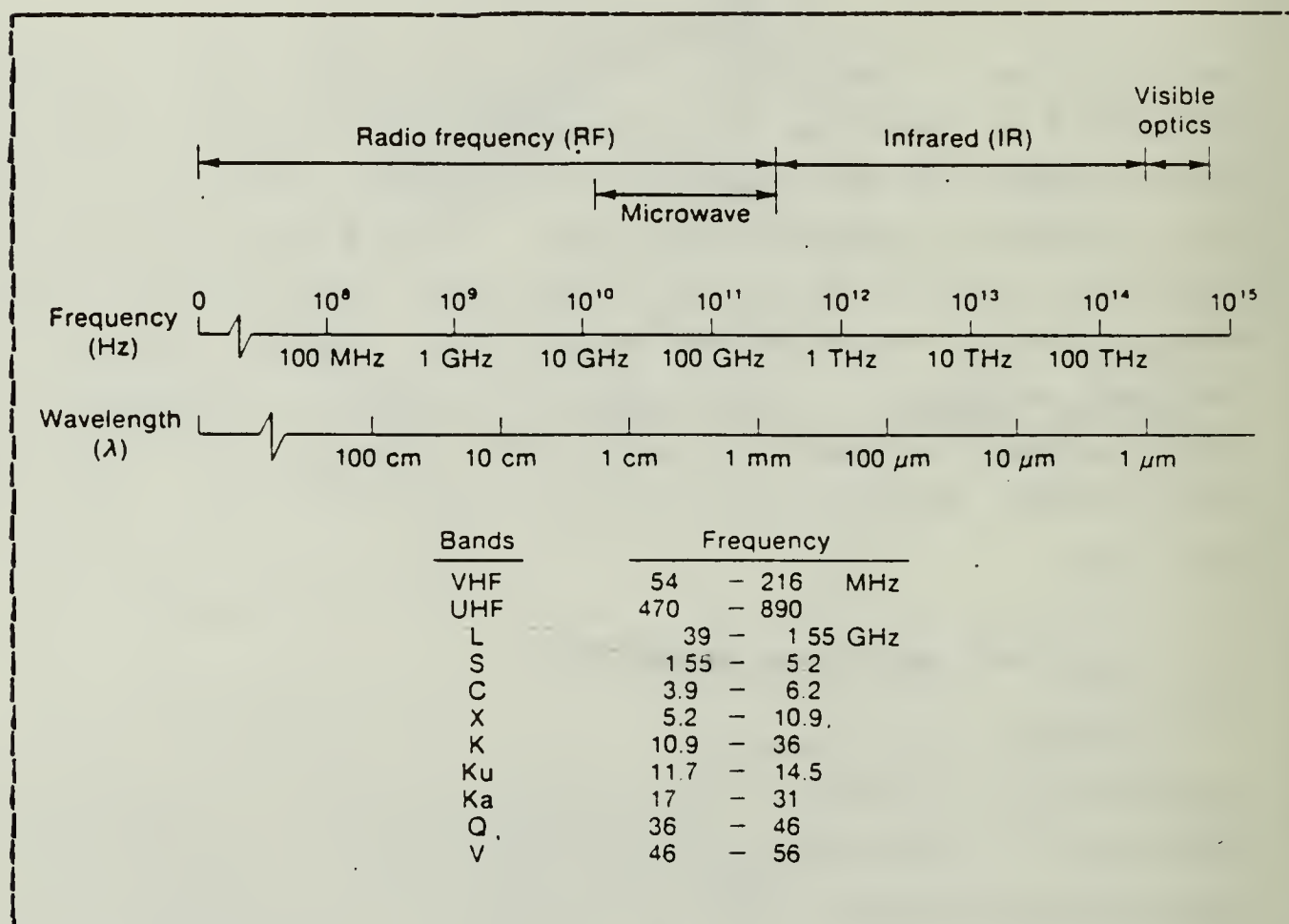


Figure 2.4 Electromagnetic Spectrum

In general, as long as the hardware and technology will support it, higher frequencies are more desirable and more in demand because they offer higher theoretical capacity. This is due to the fact that only a percentage of the carrier frequency is capable of actually transmitting a signal of a given bandwidth. Higher frequencies would also experience less interference with existing land and satellite systems. A further discussion of the bandwidths available as a function of frequency will be included at a

the time any one user has access. Finally there is code-division multiple access (CDMA) which involves modulating a specific address code which has been superimposed on the signal directly onto the carrier. In this manner all users share the satellite frequency band and only those receiving stations that can demodulate the address code can receive the specific signal. [Ref. 6]

D. WHY DIGITAL MODULATION

In general, digital signal modulation techniques are superior to analog signal modulation techniques used in satellite communications for the following reasons:

1. Compatibility with digital computers
2. Economic advantages
3. High degree of flexibility
4. Less susceptible to interference
5. Quality of signal independent of transmission distance and network makeup

1. Compatibility with Digital Computers

Clearly one of the most distinctive advantages of digital techniques over analog techniques involves computer applications. Properly formatted digital signals can be used to represent any analog signal (more on this under the discussion of the sampling theorem). Once in the digital format these signals can be easily manipulated within the digital computer. Arithmetic operations can be applied as well as logical operations. The signal can be stored without alteration or delayed and therefore can be used to "simulate" real physical situations.

The hardware associated with digital circuits is free from drift or aging and does not require calibration. Additionally digital circuitry is compatible with present day integrated circuit technology allowing a standardized

building block construction approach. The operating characteristics of these systems employing a digital computer can be changed by altering the software rather than the hardware as is the case for analog systems. Finally, the use of digital computer technology allows time multiplexing.

2. Flexibility and Economy

The flexibility and economy of digital satellite communications comes from the fact that more and more processing can be done onboard. This allows the uplink and downlink to be completely separated. This regenerative nature makes it possible for low error rates and high reliability through the use of digital techniques not available to analog systems. Because digital signal processing or multiplexing is less costly than for analog signals, simpler and cheaper interfaces between earth stations and terrestrial communications networks are possible. Additionally, there are reduced production costs and increased capacity associated with digital circuits. [Ref. 7]

3. Quality and Interference

The capability of digital systems to regenerate the signal and allow for multiple switching and signal processing without degradation in signal quality makes the digital signal basically independent of transmission distance. Multiple hops from satellite to earth station or satellite to satellite are possible without accumulation of the noise characteristic of analog systems. Additionally, digital systems are capable of operating at a signal to noise ratio of 20 dB to 30 dB as compared to analog systems requiring a much more powerful signal. [Ref. 8]

**III. INTRODUCTION TO THE FOURIER TRANSFORM, SAMPLING
THEOREM,
AUTOCORRELATION FUNCTION AND THE MATCHED FILTER**

Essential to the understanding of digital signal modulation techniques are a few basic tools of the electrical engineer and the mathematician. These tools will be developed and elaborated on to the extent necessary to understand their applicability to the subject of digital communications. The description is not meant to be a detailed investigation of the respective topics. Where relevant, the application of the concept being described will be mentioned.

A. FOURIER TRANSFORM

In mathematical terms, voltages can be expressed as functions of time or of frequency. It is more common to see voltages represented as a function of time as in equation 3.1.

$$v(t) = A \cos(\omega t) \qquad \qquad \qquad (\text{eqn 3.1})$$

A = amplitude

ω = angular frequency = $2 \pi f$

f = frequency = $1/T$

T = period

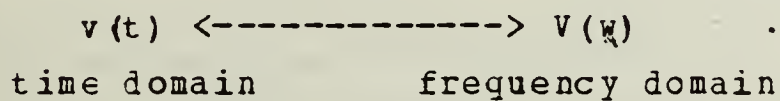
It is important to note that both the time and frequency functions are representations of voltage and as such may be used interchangeably. The Fourier representation $[v(t)] = v(f)$ is a voltage descriptor in the frequency domain (a

function of frequency) while $v(t)$ is a voltage descriptor in the time domain (a function of time). They are different but equivalent and either voltage descriptor may be used, depending on the concept being explored, to best represent the voltage within context.

The Fourier transform is of principle interest rather than the Fourier series since the latter is applicable only to periodic voltages. The Fourier transform is applicable to voltage pulses, random voltages and other non-periodic voltages.

DEFINITION:

$$\mathcal{F}[v(t)] = V(\omega) = \int_{-\infty}^{\infty} v(t) e^{-j\omega t} dt \quad (\text{eqn 3.2})$$



Remembering Euler's formula

$$e^{-j\omega t} = \cos(\omega t) - j \sin(\omega t) \quad (\text{eqn 3.3})$$

the Fourier transform becomes

$$\mathcal{F}[v(t)] = V(\omega) = \int_{-\infty}^{\infty} v(t) [\cos(\omega t) - j \sin(\omega t)] \quad (\text{eqn 3.4})$$

$$V(\omega) = \int_{-\infty}^{\infty} v(t) \cos(\omega t) - j \int_{-\infty}^{\infty} v(t) \sin(\omega t) \quad (\text{eqn 3.5})$$

Since it will be seen that digital communications deals primarily with pulses of finite duration (expressed as period, T), it is worthwhile to examine the Fourier transform of a pulse of amplitude A and duration T .

$$\text{let } v(t) = \begin{cases} A; & -T/2 < t < T/2 \\ 0; & \text{elsewhere} \end{cases}$$

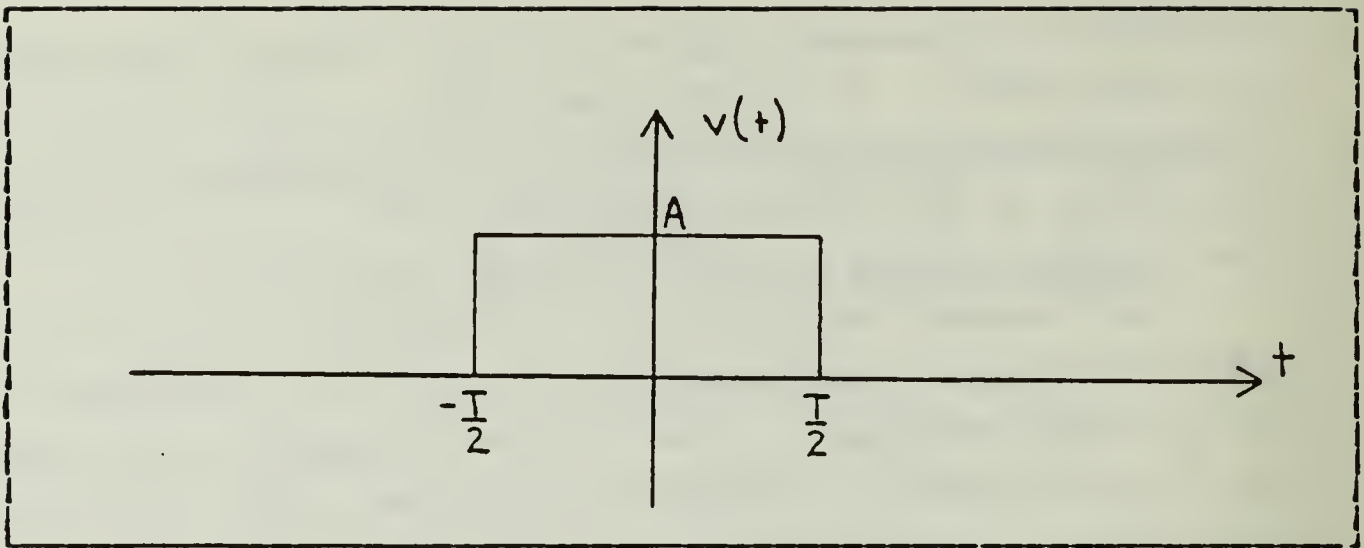


Figure 3.1 Square Pulse

Figure 3.1 is a representation of $v(t)$ or the voltage expressed in the time domain. The position of $v(t)$ on the t -axis was chosen for convenience of integration but could have been situated anywhere on the time line.

$$\mathcal{F}[v(t)] = V(\omega) = \int_{-\infty}^{\infty} v(t) e^{** -j\omega t} dt \quad (\text{eqn 3.6})$$

$$V(\omega) = \int_{-\infty}^{-T/2} 0 \cdot e^{** -j\omega t} dt + \int_{-T/2}^{T/2} A e^{** -j\omega t} dt + \int_{T/2}^{\infty} 0 \cdot e^{** -j\omega t} dt \quad (\text{eqn 3.7})$$

$$V(\omega) = \int_{-T/2}^{T/2} A e^{** -j\omega t} dt \quad (\text{eqn 3.8})$$

The integration above may be attacked either head on or by substituting $\cos(\omega t) - j \sin(\omega t)$ for $e^{** -j\omega t}$. The direct approach is illustrated due to the relative simplicity of the integrand.

$$V(\omega) = \int_{-T/2}^{T/2} A e^{** -j\omega t} dt \quad (\text{eqn 3.9})$$

$$V(\omega) = -A/j\omega [e^{** -j\omega t}] \Big|_{-T/2}^{T/2} \quad (\text{eqn 3.10})$$

$$V(\omega) = -A/j\omega[e^{-j\omega T/2} - e^{j\omega T/2}] \quad (\text{eqn 3.11})$$

$$V(\omega) = A/j\omega[e^{j\omega T/2} - e^{-j\omega T/2}] \quad (\text{eqn 3.12})$$

By substituting $2\pi f = \omega$, the following result is obtained:

$$V(f) = A/j2\pi f[e^{j2\pi fT/2} - e^{-j2\pi fT/2}] \quad (\text{eqn 3.13})$$

$$V(f) = A/j2\pi f[e^{j\pi fT} - e^{-j\pi fT}]$$

Using Euler's formula, i.e., $\sin \theta = (e^{j\theta} - e^{-j\theta})/2j$:

$$V(f) = 2jA/j2\pi f[(e^{j\pi fT} - e^{-j\pi fT})/2j] \quad (\text{eqn 3.14})$$

$$V(f) = A/\pi f[\sin(\pi fT)]$$

Knowing that $\sin x / x = \text{sinc } x$

$$V(f) = AT/\pi fT[\sin(\pi fT)] \quad (\text{eqn 3.15})$$

$$V(f) = AT \text{sinc}(\pi fT)$$

The sinc function is common in digital electronics and plots as the product of $\sin(\pi fT)$ and $1/(\pi fT)$ as in Figure 3.2. In Figure 3.2, $V(f)$ in the frequency domain is equivalent to $v(t)$ in the time domain. Note that as the pulse, T , gets longer, $1/T$ gets smaller or the first zero crossing of the sinc function occurs at a lower and lower frequency.

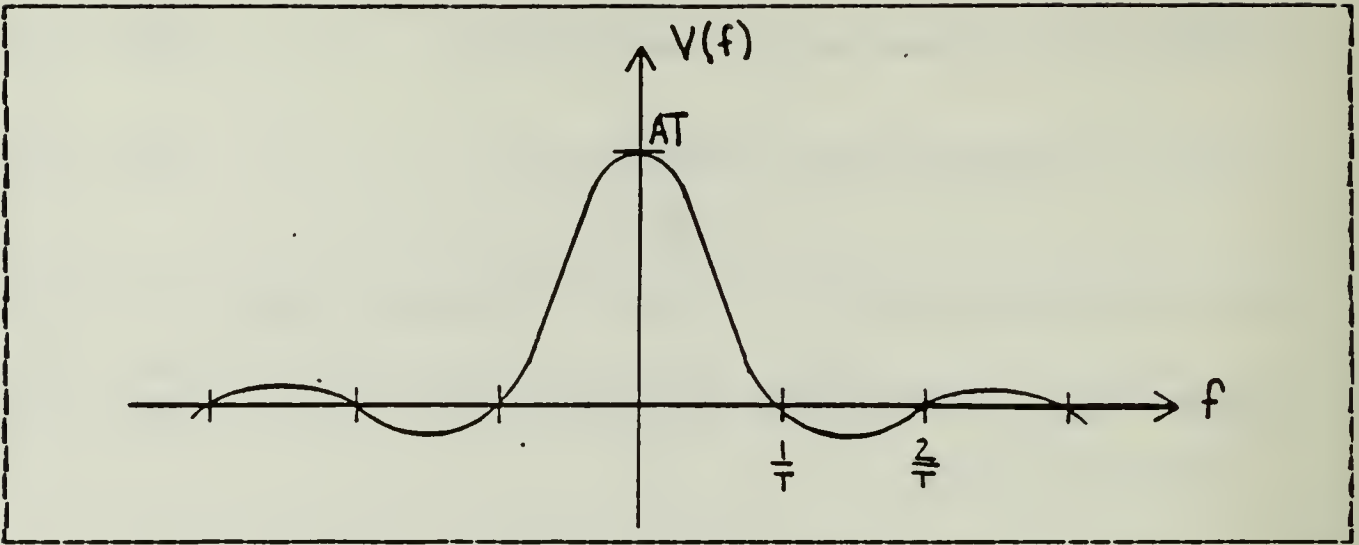


Figure 3.2 Plot of Sinc Function

1. Amplitude and Phase Spectrum

Recall that $V(\omega)$ can be represented as in equation 3.16. The cosine term is the real part while the sine term is the imaginary part. By referencing Figure 3.3, a brief review of the complex plane is accomplished and its relationship to the amplitude and phase spectrum of a given voltage is represented. See equations 3.17 through 3.20.

$$V(\omega) = \int_{-\infty}^{\infty} v(t) \cos(\omega t) dt - j \int_{-\infty}^{\infty} v(t) \sin(\omega t) dt \quad (\text{eqn 3.16})$$

real
imaginary

$|V(f)|$ is called the amplitude spectrum of the given voltage. The amplitude spectrum can also be calculated by using the complex conjugate of the Fourier transform and is always positive as shown in equation 3.21. The phase spectrum, θ , of the function in question is represented by the $\arctan[\text{imaginary}/\text{real}]$ and is illustrated in Figure 3.5.

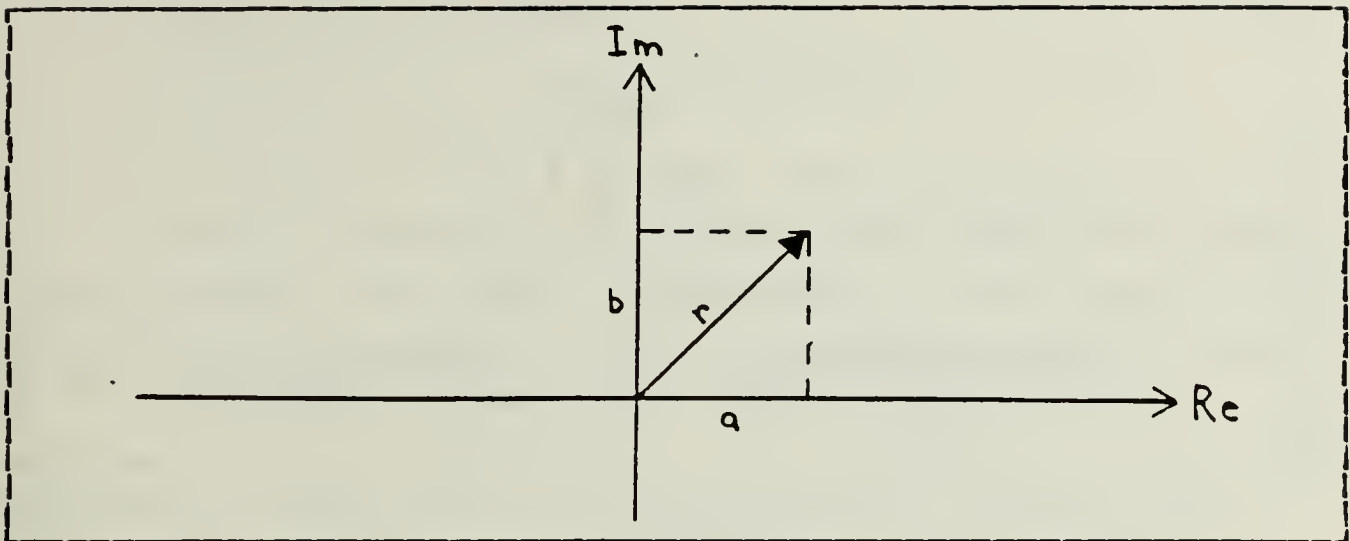


Figure 3.3 Phasor Diagram

$$r = [a^2 + b^2] \quad (\text{eqn 3.17})$$

$$a + jb = [a^2 + b^2]^{.5} e^{j\theta} \quad (\text{eqn 3.18})$$

$$V(f) = [\text{real}^2 + \text{imaginary}^2]^{.5} e^{j\theta} \quad (\text{eqn 3.19})$$

$$|V(f)| = [\text{real}^2 + \text{imaginary}^2]^{.5} \quad (\text{eqn 3.20})$$

since $|e^{j\theta}| = 1$

$$|V(f)| = [V(f) \cdot V^*(f)]^{.5} \quad (\text{eqn 3.21})$$

2. Properties of the Fourier Transform

Several properties of the Fourier transform are useful in the study of digital signals. They are represented here without proof and without a great deal of detail.

a. Linearity

if $v_1(t) \leftrightarrow V_1(f)$ and

if $v_2(t) \leftrightarrow V_2(f)$ then

$$\mathcal{F}[av_1(t) + bv_2(t)] = aV_1(f) + bV_2(f)$$

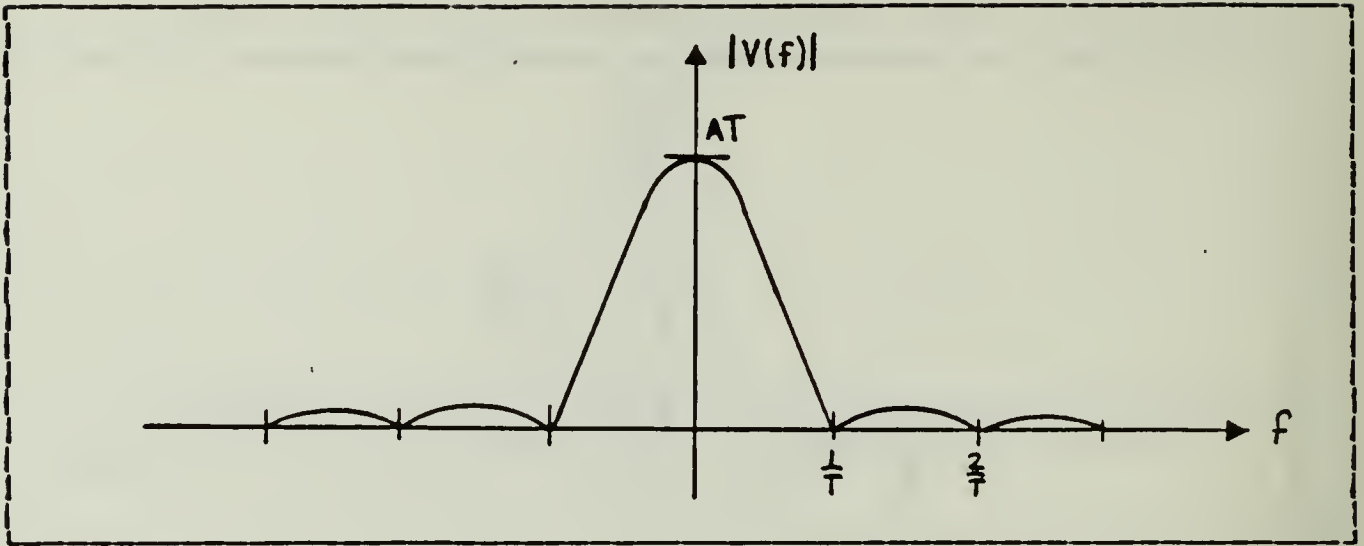


Figure 3.4 Amplitude Spectrum of Square Wave

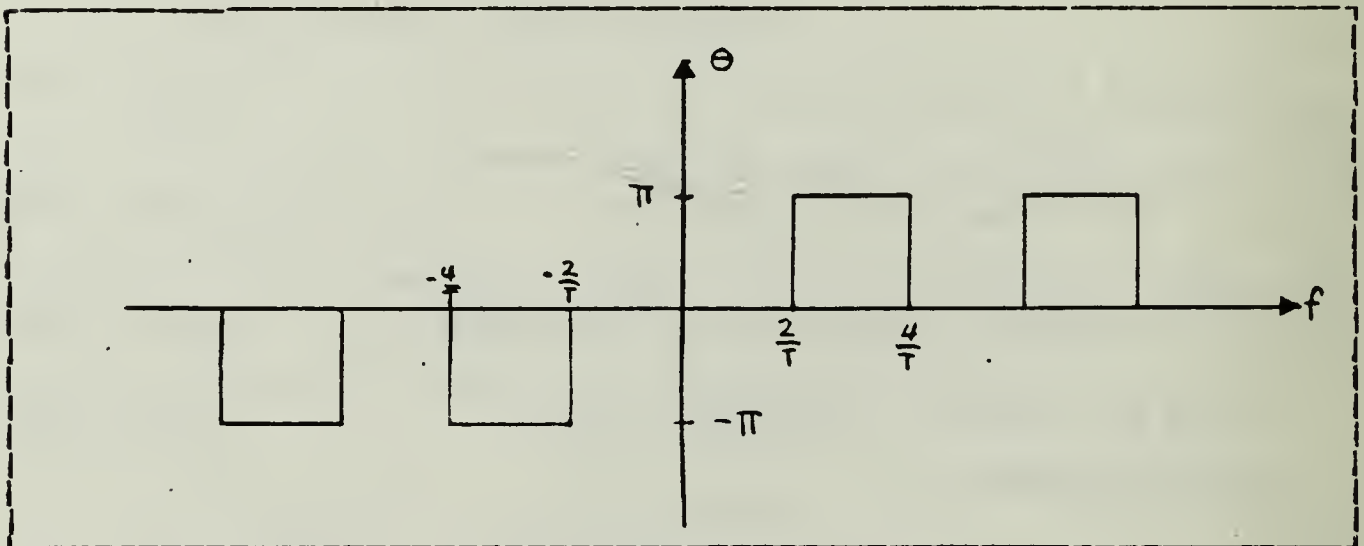


Figure 3.5 Phase Spectrum of Square Wave

b. Time-delay

$$\mathcal{F}[v(t-t_0)] = V(f) e^{-j\omega t_0}$$

Note that the amplitude spectrum of the delayed version is the same as the amplitude spectrum of the undelayed version. It is comforting to note that the Fourier transform of a pulse is the same tomorrow as it is today.

c. Scale change

$$\mathcal{F}[v(at)] = 1/|a| V(f/a)$$

d. Frequency translation

$$v(t) \cos(2 \pi f_c t) \leftrightarrow \frac{1}{2}[V(f+f_c) + V(f-f_c)]$$

$v(t)$ is any voltage

$\cos(2 \pi f_c t)$ is a carrier wave of frequency f_c

Since understanding of this very important property of the Fourier transform is essential to the understanding of digital signal modulation it is expanded slightly here.

As we have seen, the Fourier representation of a voltage pulse of amplitude A and duration T is the sinc function of amplitude AT as illustrated in Figure 3.6.

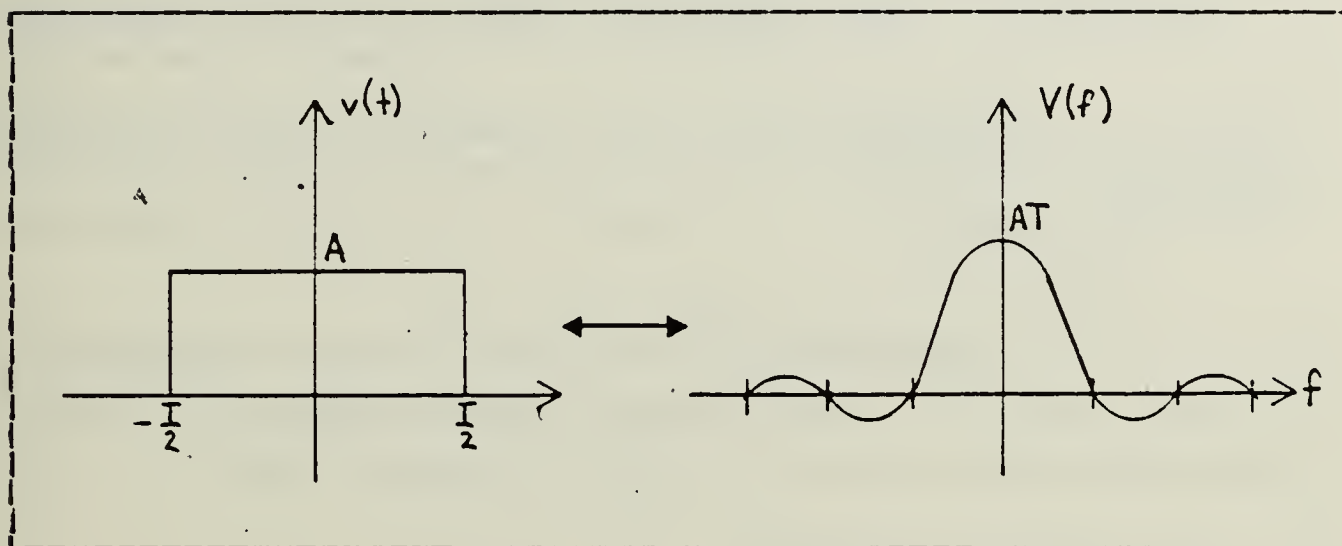


Figure 3.6 Square Wave in Time/Sinc Function in Frequency

The translation is the product of $v(t)$ and in this case $\cos(2 \pi f_c t)$. In the time domain this product only exists in the interval between $-T/2$ and $T/2$ as in Figure 3.7. The significance of this translation and its relationship to the bandwidth of the voltage will be discussed further in the section dealing with bandwidth.

e. Differentiation

$$d v(t)/dt \leftrightarrow j \omega V(f)$$

A differentiator could be used as a clock for timing but would never be used in the presence of noise since the

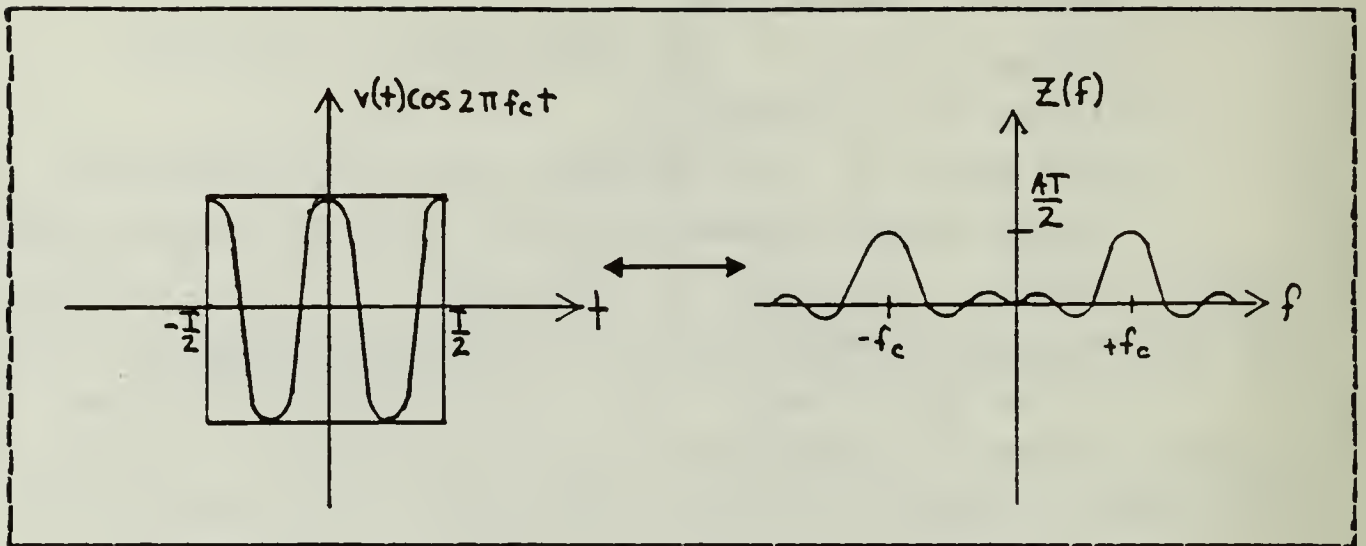


Figure 3.7 Multiplication and Translation Diagrams

result is exaggerated in the presence of high frequencies because $\omega = 2\pi f$.

f. Integration

$$v(t) dt \leftrightarrow 1/\omega V(f)$$

An integrator could be used to reduce the effects of noise since $\omega = 2\pi f$ is in the denominator tending to deemphasize the presence of high frequency noise.

B. THE SAMPLING THEOREM

Essential to the understanding of digital communications is the sampling theorem which was first introduced by Nyquist in 1928 [Ref. 9], and later by Shannon in 1948 [Ref. 10]. The sampling theorem states that any voltage can be uniquely represented by appropriately spaced sample values of the original voltage. More correctly stated, the sampling theorem places limits on the accuracy with which a signal can be represented.

The implication is that an analog signal can be represented digitally or by a set of numbers, i.e., samples. A description of the sampling theorem follows.

Given any analog voltage, $v(t)$ as in Figure 3.8, the sampling theorem says that the entire analog signal is not required to accurately represent the voltage but only samples of it, call them $v_s(t)$. Figure 3.9 shows samples of a representative analog voltage. Samples can be taken of $v(t)$ at every T seconds for a period of seconds. This can be accomplished by the use of a voltage clock, call it $v_c(t)$. The sampling can be viewed graphically as a block diagram representing an analog voltage multiplier as shown in Figure 3.10. To be of further use in the understanding of digital communications we are interested in a frequency description of the sample voltage, $v_s(t)$. Note that the system which describes the obtaining of $v_s(t)$ involves a voltage multiplication. It was demonstrated in the proceeding section that voltage multiplication amounted to frequency translation, a property of the Fourier transform.

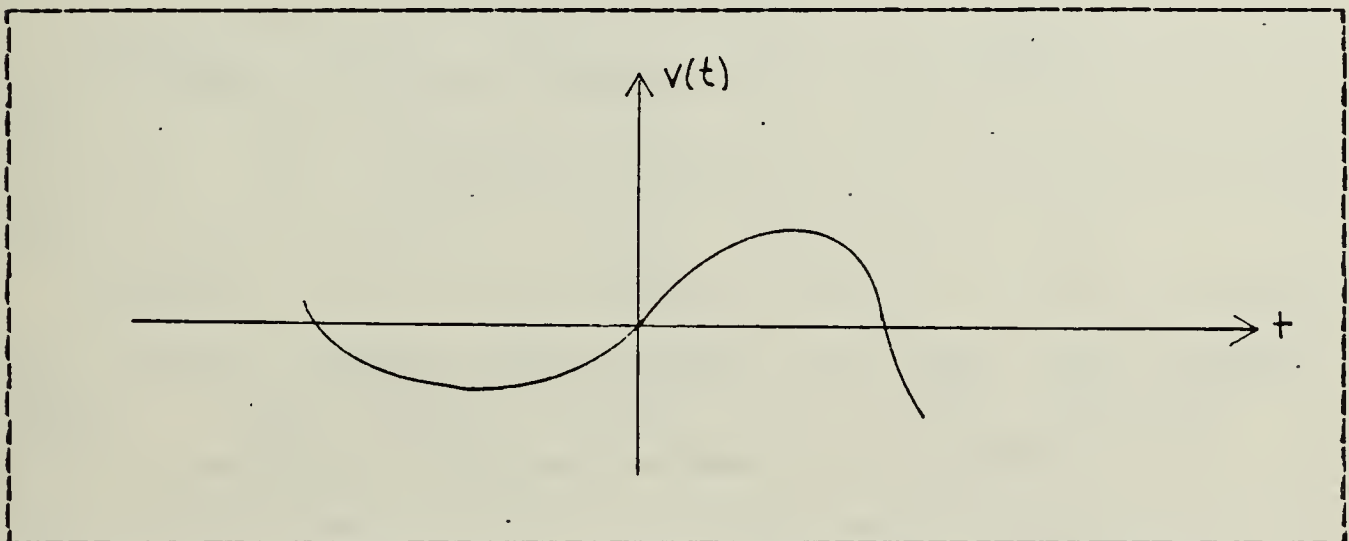


Figure 3.8 Representative Analog Voltage

First it is necessary to find the frequency description of the clock, $v_c(t)$, Let $v_c(t)$ be a periodic square wave of height 1 and duration d as in Figure 3.11. Since $v_c(t)$ is periodic, it can be shown that the Fourier series representing $v_c(t)$ is given by equation 3.22.

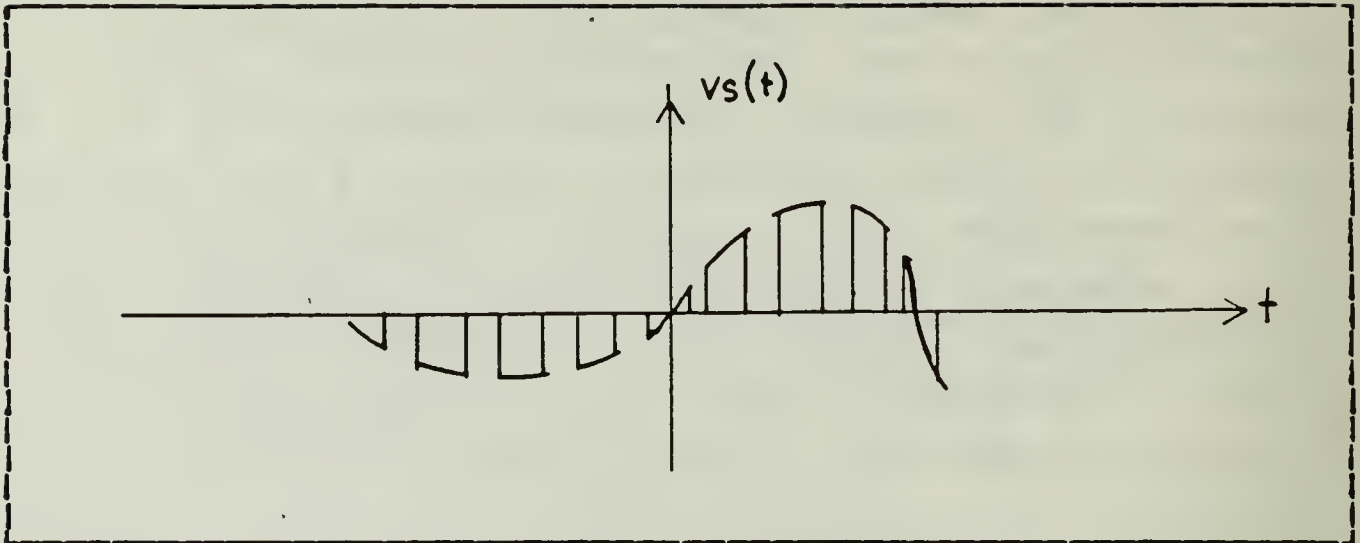


Figure 3.9 Samples of a Representative Voltage

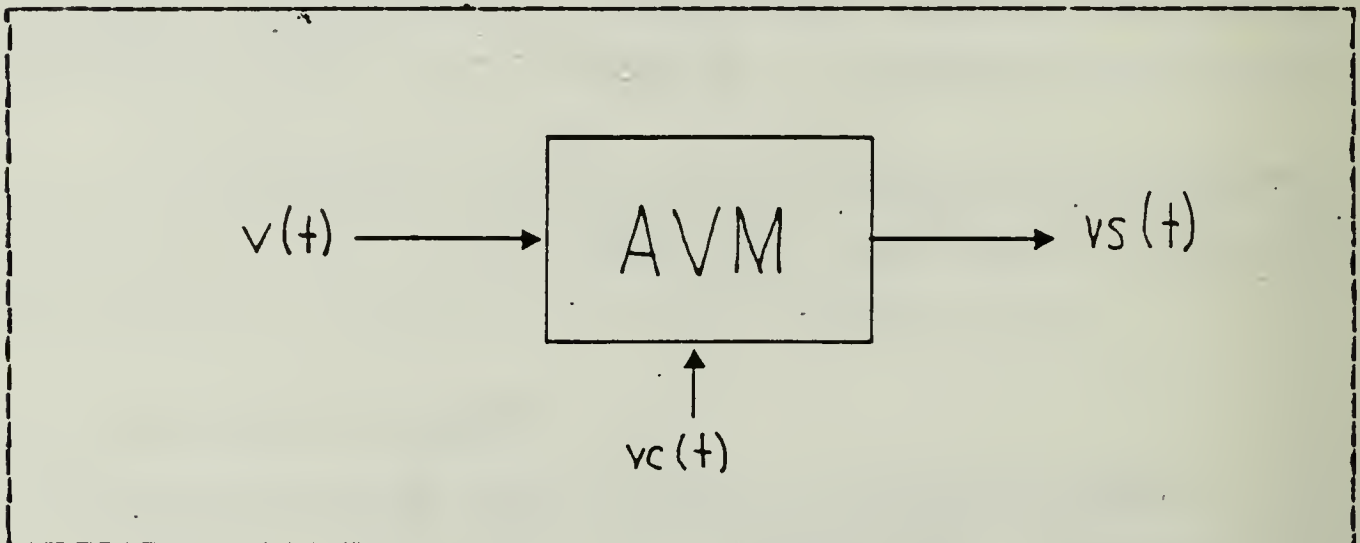


Figure 3.10 Analog Voltage Multiplier

Again it is noted that $v_s(t)$, the sample voltage, is the product of $v(t)$, the original analog voltage, times $v_c(t)$, the clock voltage. In other words $v_s(t) = v(t)$ times a series of cosine terms.

$$v_c(t) = a_0 + \sum_{n=1}^{\infty} a_n \cos(2 \pi n f_c t) \quad (\text{eqn 3.22})$$

a_0 and a_n are left unevaluated

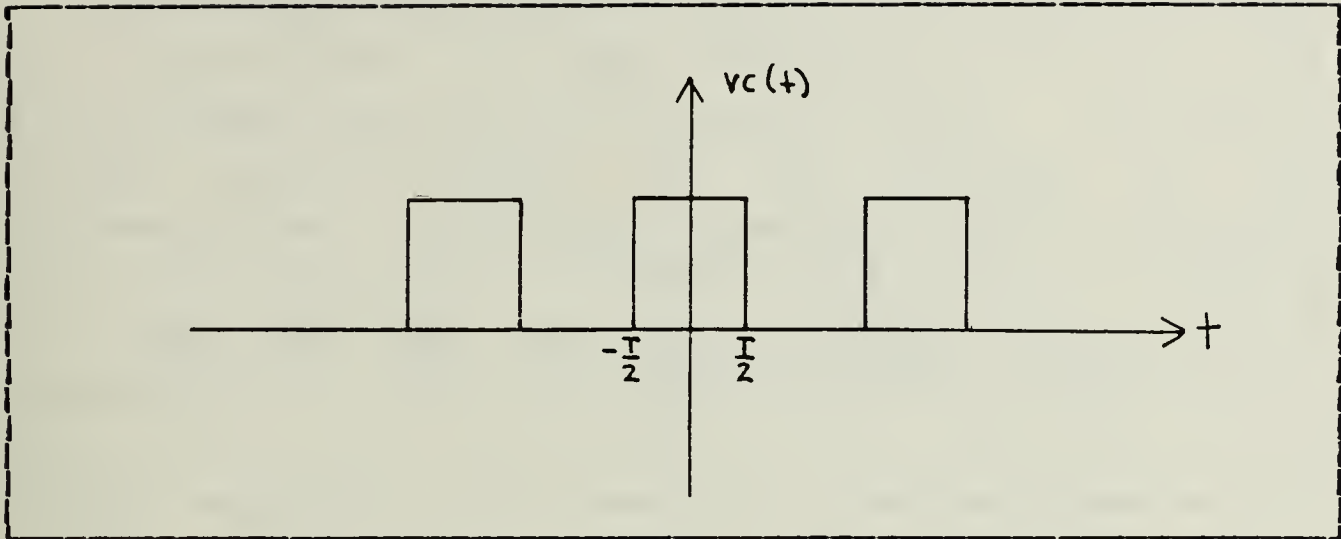


Figure 3.11 A Representative Voltage Clock

$$v_s(t) = v(t) \left[a_0 + \sum_{n=1}^{\infty} a_n \cos(2 \pi n f_c t) \right] \quad (\text{eqn 3.23})$$

Now, assuming any form of the Fourier transform of $v(t)$, as in Figure 3.12 and since $v_s(t)$ is a product and by utilizing the frequency translation property of the Fourier transform, the following is obtained as a representation of the frequency spectrum of $v_s(t)$. See Figure 3.13.

Remember that the curve highlighted in the box in Figure 3.13 is the Fourier representation of $v(t)$, the original signal. This original signal can now be recovered by filtering with an appropriate low pass filter of bandwidth equal to or greater than B . This low pass filter would only permit the reception of that portion of the signal which represents the original voltage.

The only question left to resolve is how often to take a sample. Again referring to the diagram in Figure 3.13, it is noted that in order to prevent any overlap of successive translations (aliasing)

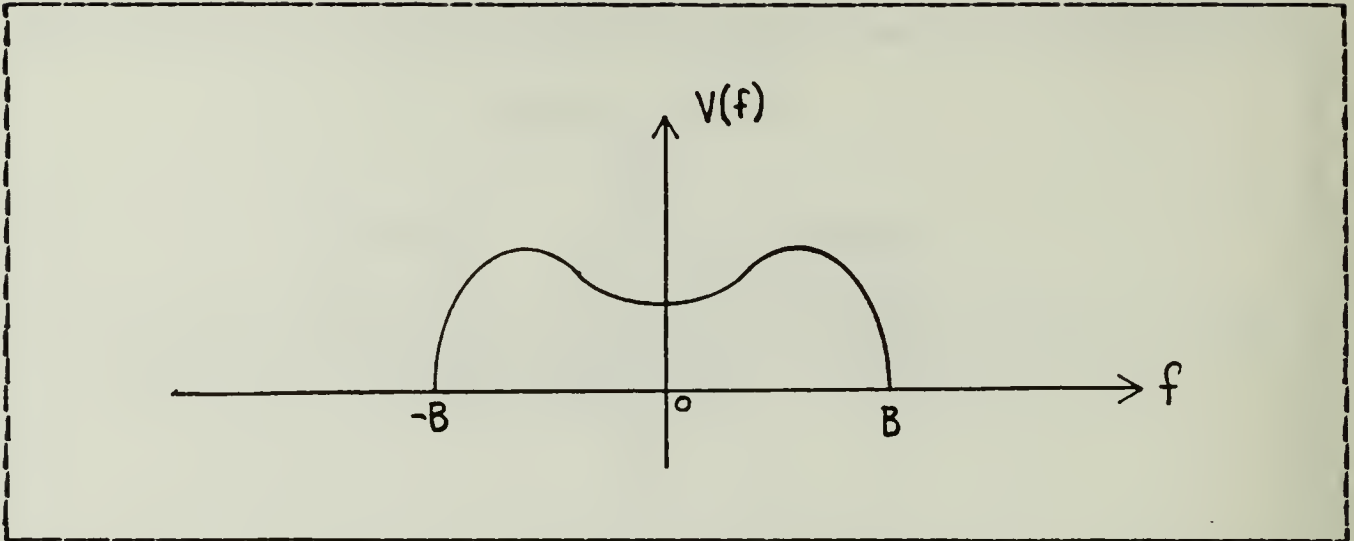


Figure 3.12 Fourier Transform of $v(t)$

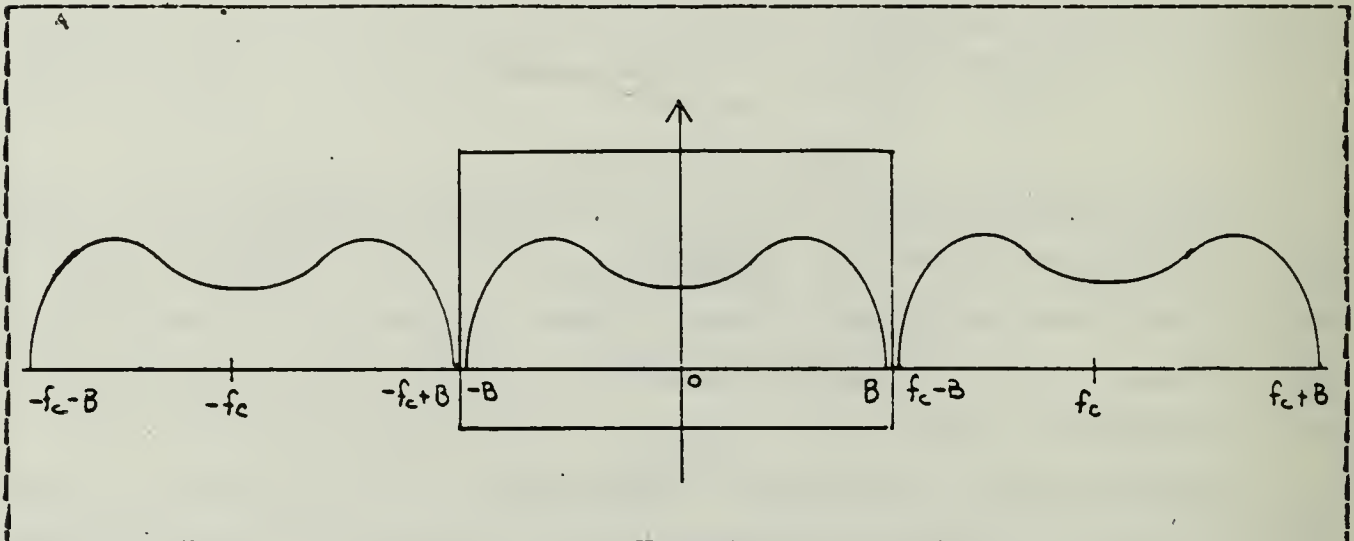


Figure 3.13 Fourier Transform of $v_s(t)$

$$f_0 - B \gg B$$

$$f_0 \gg 2B$$

or the frequency of the clock, f_c (the sampling rate = $1/T$) must be strictly greater than 2 times the largest significant Fourier frequency component present. Since B will vary with different $v(t)$, the sampling rate necessary to uniquely recover that $v(t)$ also varies.

In summary on the sampling theorem, it can be said that any analog signal can be represented as certain sample values spaced the appropriate distance apart. The sampling theorem places limits on the accuracy of this representation. These sample values can then be transmitted from one position to another using analog to digital conversion and any one of a variety of modulation techniques. It has been shown that the Fourier frequency representation of the sample is not equivalent to the Fourier frequency representation of the source voltage; however, the source voltage can be recovered at the receiving end by filtering. A block representation of the system is shown in Figure 3.14.

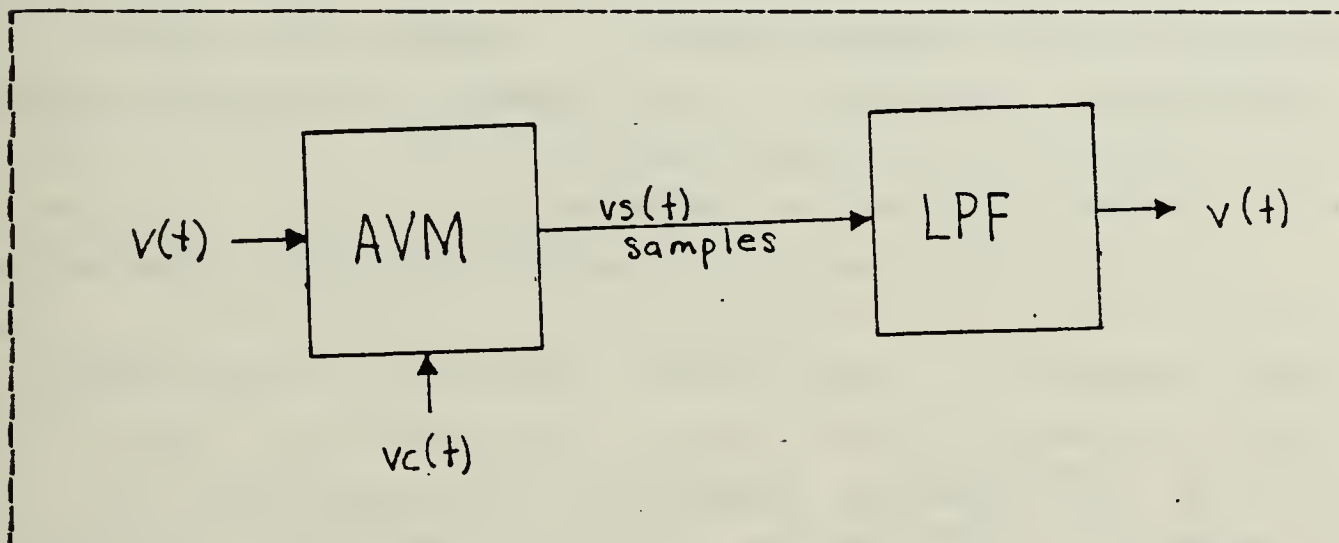


Figure 3.14 Analog Voltage Multiplier and Low Pass Filter

C. THE AUTOCORRELATION FUNCTION

The above concept certainly seems simple enough. If a signal is present and it is desired to transmit it from point A to point B, all that has to be done is to take appropriately spaced samples of the signal, encode them,

somehow transmit them to point B, filter the received signal and the uniqueness of the original voltage has been reproduced. Unfortunately it isn't quite that easy. The reason it is not, is due to the presence of noise. The sources of noise will not be discussed here, however, the effects of noise in general terms and how a faint signal can be recovered in the presence of noise will be discussed.

The time varying descriptor of voltage and the frequency varying descriptor of voltage have been introduced. Both are precise mathematical descriptions of something (voltage) that is deterministic. That is, it can be described in mathematical or graphical terms during any period of time. Such is not the case for noise corrupted voltages which are entirely random. Therefore other descriptors of voltages must be employed in the presence of noise. They are partial descriptors of voltage since a random signal cannot be described with precision. These partial descriptors are the

1. Autocorrelation function and the
2. Probability density function (p.d.f.)

It is important here to note the difference between the source voltage at the receiver and the sample voltage. The source voltage at the receiver, $v_{sr}(t)$, is the digitally converted sample voltage, $v_s(t)$, modulated onto a carrier by one of the digital modulation techniques yet to be discussed. Understanding the autocorrelation function is the basis for understanding how a decision is made that $v_{sr}(t)$ is present at the receiver in the presence of noise. It should be remembered that the exact form of the carrier is known at both the transmitter and receiver.

First of all, an additive noise model is assumed where the signal at the receiver, $v_r(t)$, is equal to the signal which is being transmitted, $v_{sr}(t)$, (i.e., the digital samples of $v(t)$ modulated onto the carrier), plus random noise, $v_n(t)$

$$v_r(t) = v_{sr}(t) + v_n(t) \quad (\text{eqn 3.24})$$

$v_r(t)$ = voltage at the receiver

$v_{sr}(t)$ = signal voltage at the receiver

$v_n(t)$ = noise voltage at the receiver

If it is realized that most receivers operate on the principle of detection of DC voltage, the problem becomes one of rectification of the received signal and determination of the DC voltage, characteristic of the transmitted signal is present.

A common type of rectification of an analog voltage involves squaring the input waveform. If the given signal at the receiver is $v_r(t)$ as in equation 3.24 above, squaring the waveform introduces the square of not only the desired signal but also the square of the noise term. If instead of squaring $v_r(t)$ and introducing or at least not eliminating the noise, $v_r(t)$ is multiplied by $v_{sr}(t)$, the results in equation 3.25 are obtained.

$$v_r(t) \cdot v_{sr}(t) = v_{sr}^2(t) + v_{sr}(t)v_n(t) \quad (\text{eqn 3.25})$$

By averaging, all that remains is $\overline{v_{sr}^2(t)}$ since the average of $v_{sr}(t)v_n(t)$ is zero because $\overline{v_n(t)}$ is random and the average of any random voltage is zero. The DC component of $v_r(t) \cdot v_{sr}(t)$ is $\overline{v_{sr}^2(t)}$. Any remaining AC component can be removed by a low pass filter. Graphically in block diagram form this receiver looks like Figure 3.15 illustrated below. If $\overline{v_{sr}^2(t)} > 0$ then $v_{sr}(t)$ is present in the signal $v_r(t)$. If $v_r(t)$ is pure noise or some other signal is present exclusively, then the output of the receiver will be 0.

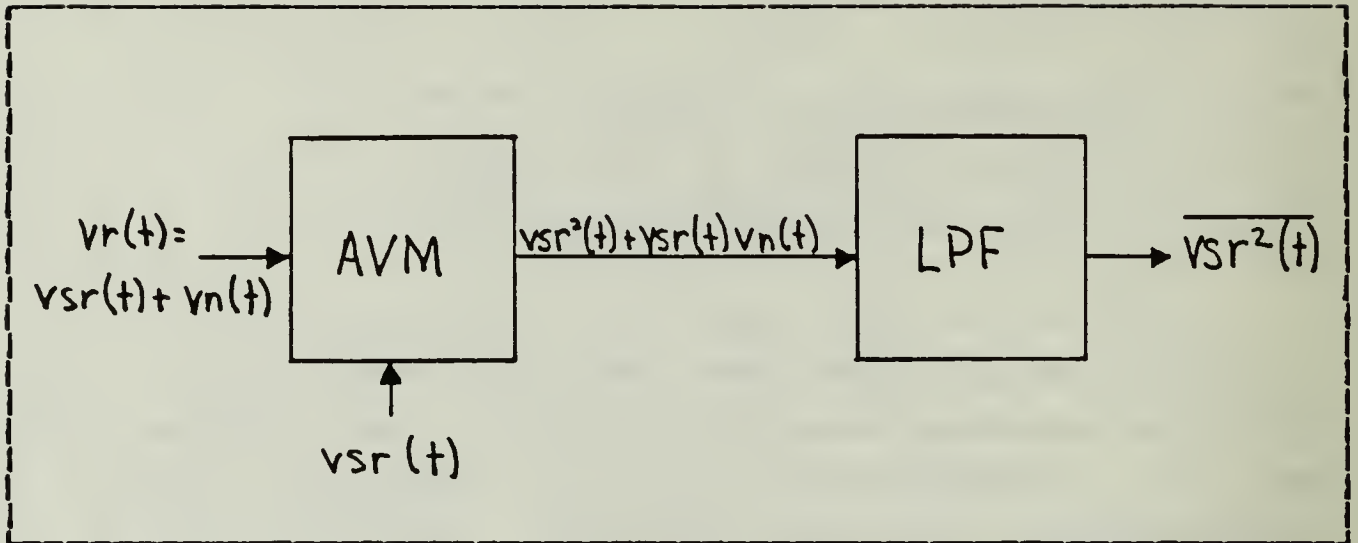


Figure 3.15 Rectification through an AVM and LPF

In practice, however, the exact waveform of $v_{sr}(t)$ may not be known or it may be a time delayed or distorted version of the original signal when it arrives at the receiver. If the distortion or delay is significant enough there will be little agreement or "correlation" in the receiver.

The solution is to multiply the received signal by a series of time delayed approximations of the transmitted signal. The signal is present whenever the output of the series of voltage multipliers or correlators exceeds a certain threshold approaching $v_{sr}^2(t)$. The concept is illustrated in Figure 3.16.

For the concept illustrated in Figure 3.16 to work, the average value of $v_r(t) \cdot v_{sr}(t-p)$ must have a DC component.

$$v_r(t) \cdot v_{sr}(t-p) = v_{sr}(t)v_{sr}(t-p) + v_n(t)v_{sr}(t-p) \quad (\text{eqn 3.26})$$

$$\overline{v_r(t) \cdot v_{sr}(t-p)} = \overline{v_{sr}(t)v_{sr}(t-p)} + \overline{v_n(t)v_{sr}(t-p)} \quad (\text{eqn 3.27})$$

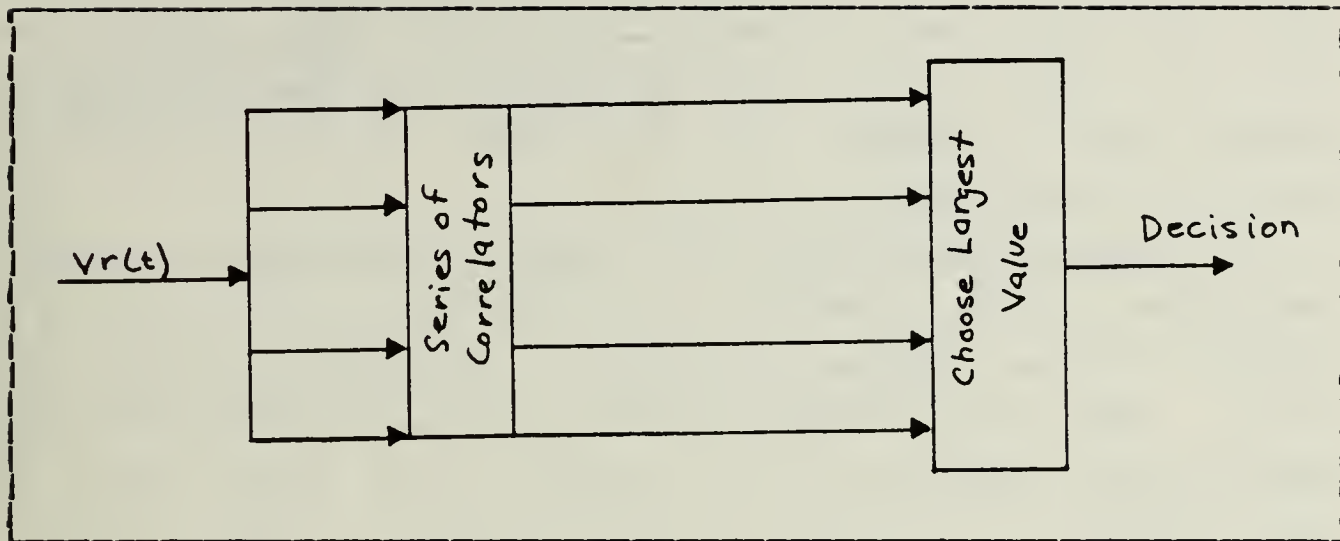


Figure 3.16 Correlation Device

But the average of $v_n(t) v_{sr}(t-p) = 0$ since $\overline{v_n(t)}$ is random and the results of equation 3.28 are obtained.

$$\overline{v_r(t) \cdot v_{sr}(t-p)} = \overline{v_{sr}(t) v_{sr}(t-p)} \quad (\text{eqn 3.28})$$

What is of interest is the average value of $v_{sr}(t) v_{sr}(t-p)$. The autocorrelation function (ACF) will be defined as that average value of $v_{sr}(t) v_{sr}(t-p)$. The mathematical representation of the autocorrelation function for a continuous voltage is represented in equation 3.29 while the autocorrelation function for a pulse voltage is presented as equation 3.30.

$$\text{ACF} = R_{vv}(p) = \frac{1}{2T} \int_{-T}^T v(t) v(t-p) dt \quad (\text{eqn 3.29})$$

$$\text{ACF} = C_{vv}(p) = \int_{-\infty}^{\infty} v(t) v(t-p) dt \quad (\text{eqn 3.30})$$

The autocorrelation function is a measure of the degree to which two identical signals which are corrupted in some manner are alike. The ACF of two signals which are identical, not distorted in any way and occurring at exactly

the same time, i.e., $p = 0$ has a maximum value. On the other hand there will be very little correlation between two identical time variant signals when the time difference between them is great. In this case the autocorrelation function is near zero.

A similar concept is used within the context of signal comparison. This concept is the crosscorrelation which is a measure of the degree to which 2 different signals are alike. When the crosscorrelation between voltage v_{sr} and random noise voltage v_n is 0 there is no relationship or correlation.

Again let us assume that the signal at the receiver is a noise disrupted version of the signal originally transmitted.

$$v_r(t) = v_{sr}(t) + v_n(t) \quad \text{(eqn 3.31)}$$

In the receiver, the time delayed version of the signal is applied to the incoming signal and the average is formed as before and shown in Figure 3.17.

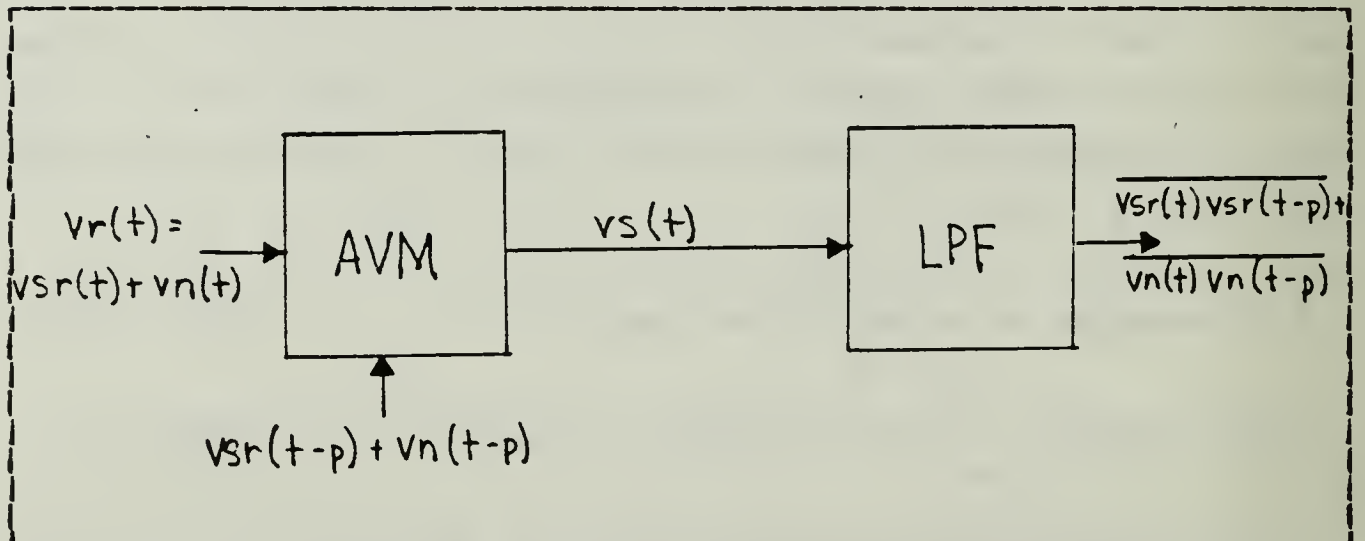


Figure 3.17 Voltage Correlator

$$\begin{aligned} & \overline{[v_{sr}(t) + v_n(t)] \cdot [v_{sr}(t-p) + v_n(t-p)]} = & \text{(eqn 3.32)} \\ & \overline{v_{sr}(t)v_{sr}(t-p)} + \overline{v_n(t)v_{sr}(t-p)} + \\ & \overline{v_{sr}(t)v_n(t-p)} + \overline{v_n(t)v_n(t-p)} = \end{aligned}$$

$$R_{v_{sr} v_{sr}}(p) + R_{v_n v_{sr}}(p) + R_{v_{sr} v_n}(p) + R_{v_n v_n}(p)$$

$$R_{v_n v_{sr}}(p) = 0$$

$$R_{v_{sr} v_n}(p) = 0; \text{ because average } v_n = 0$$

Therefore the result is simply $R_{v_{sr}} = v_{sr}(p) + R_{v_n v_n}(p)$ or the autocorrelation function of the desired signal plus the autocorrelation function of the noise. Assuming the shape of the autocorrelation function of both components (both the original signal and the noise which vary with p , time) is known, what is done in practice is to vary the value of p until the ratio of $R_{v_{sr} v_{sr}}(p) / R_{v_n v_n}(p)$ is a maximum or the autocorrelation function of the signal is a maximum while the autocorrelation of the noise is minimum and the signal is recovered.

D. THE MATCHED FILTER

The matched filter is a linear filter which has the characteristic response desired for optimum reception of the desired signal. In other words, we desire the response of the system to the linear filter to be in some way proportional to the autocorrelation function of the desired signal and in no way related to the autocorrelation function of the noise. This system could be illustrated as in Figure 3.18.

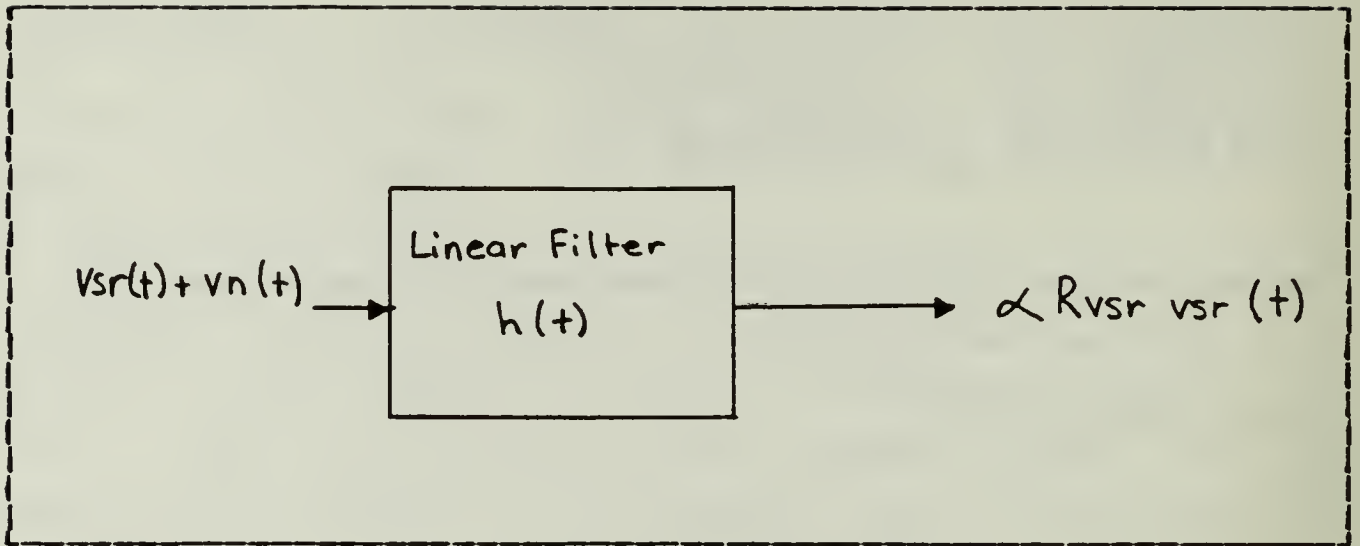


Figure 3.18 Matched Filter Block Representation

The question is what should the makeup or $h(t)$, (i.e., the response of the linear filter) be? The output of a linear system is a convolution so the output of the linear filter, $h(t)$ to an input $v_{sr}(t)$ would be $v_{sr}(t) * h(t)$, where $*$ denotes convolution.

In the previous section it was stated that the autocorrelation function, $R_{v_{sr}} v_{sr}(p)$, a function of p , is given by

$$R_{v_{sr}} v_{sr}(p) = \int_{-\infty}^{\infty} v_{sr}(t) v_{sr}(t-p) dt \quad (\text{eqn 3.33})$$

By simply changing variables, equation 3.33 can be rewritten as a function of time, t .

$$R_{v_{sr}} v_{sr}(t) = \int_{-\infty}^{\infty} v_{sr}(p) v_{sr}(p-t) dp \quad (\text{eqn 3.34})$$

From convolution theory it is known that the response of a linear filter as above, $v_{sr}(t) * h(t)$ can be expressed mathematically as in equation 3.35.

$$v_{sr}(t) * h(t) = \int_{-\infty}^{\infty} v_{sr}(p) h(t-p) dp \quad (\text{eqn 3.35})$$

As stated earlier, the desired output of the linear filter is the autocorrelation function $R_{v_{sr}}(t)$. Note the similarities between the last two equations. If in equation 3.35 a simple substitution of $h(t) = v_{sr}(-t)$ is performed, the desired results are obtained.

$$v_{sr}(t) * h(t) = \int_{-\infty}^{\infty} v_{sr}(p) v_{sr}(p-t) dp \quad (\text{eqn 3.36})$$

$$= R_{v_{sr}}(t)$$

Therefore, for every signal that is desired to be recovered, the matched filter will do the job very nicely if the response of that filter, $h(t)$ is equal to the inverse of the signal that is desired to be detected.

IV. ANALOG TO DIGITAL CONVERSION

Key to the understanding of digital communications is how the analog information is converted to digital information. As illustrated earlier, each analog voltage or signal can be represented by appropriately spaced sample values. These sample values are still analog in that they can take on any value in the range of the original analog signal. What is desired is to change this infinite set of decimal numbers to a finite set of decimal numbers. This is called analog to digital conversion. Common types of A to D conversion include Pulse Code Modulation (PCM), Differential Pulse Code Modulation (DPCM), Delta Modulation (DM), Pulse Amplitude Modulation (PAM), Pulse Duration Modulation (PDM), and Pulse Position Modulation (PPM). PCM, DPCM, and DM will be examined in this chapter because of their widespread usage and easy application to digital technology.

A. PULSE CODE MODULATION (PCM)

PCM is the most widely used A to D conversion technique. It involves assigning the sample value obtained in sampling to one of several quantization levels within the range of the voltage sampled and then representing those quantization levels by various binary code words.

For example, the highest significant frequency component in human speech is 3300 Hz. In order to capture accurately the signal produced in speech, one would require a sampling rate greater than or equal to $2B$ or $2(3300) = 6600$ samples/sec. The telephone company uses 8000 samples/sec.

$$B = 3300 \text{ Hz}$$

$$f \geq 2B = 6600 \text{ samples/sec}$$

use $f = 8000$ samples/sec to ensure no aliasing

If a signal is sampled at the rate of 8000 samples/sec, then in the transmission of those samples, assuming the samples are transmitted immediately and not delayed, the transmission rate must be

$$T_s = 1/f$$

$$T_s = 1/8000 \text{ samples/sec}$$

$$T_s = 125 \text{ microsec/sample}$$

The number of quantization levels employed to represent the various analog sample values is arbitrary. The greater the number of levels, the more accurate the reconstruction of the original signal but the more rapid the data transmission rate must be (in all cases there will be some error present after recovery). Consider again the example of voice as illustrated in Figure 4.1.

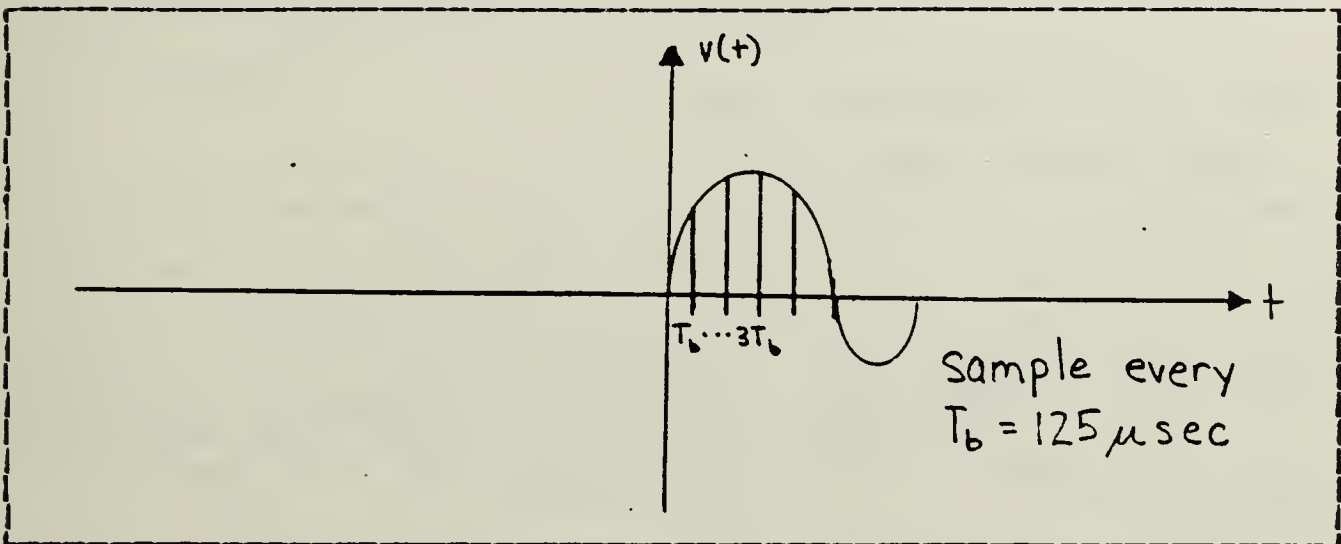


Figure 4.1 Samples of Voltage

Assume it is desired to represent each sample value (decimal number) with an 8 bit binary code word. Then the number of quantization levels is given by equation 4.1.

The spacing between quantization levels is the range of voltages to be represented divided by the number of quantization levels. The analog to digital conversion takes

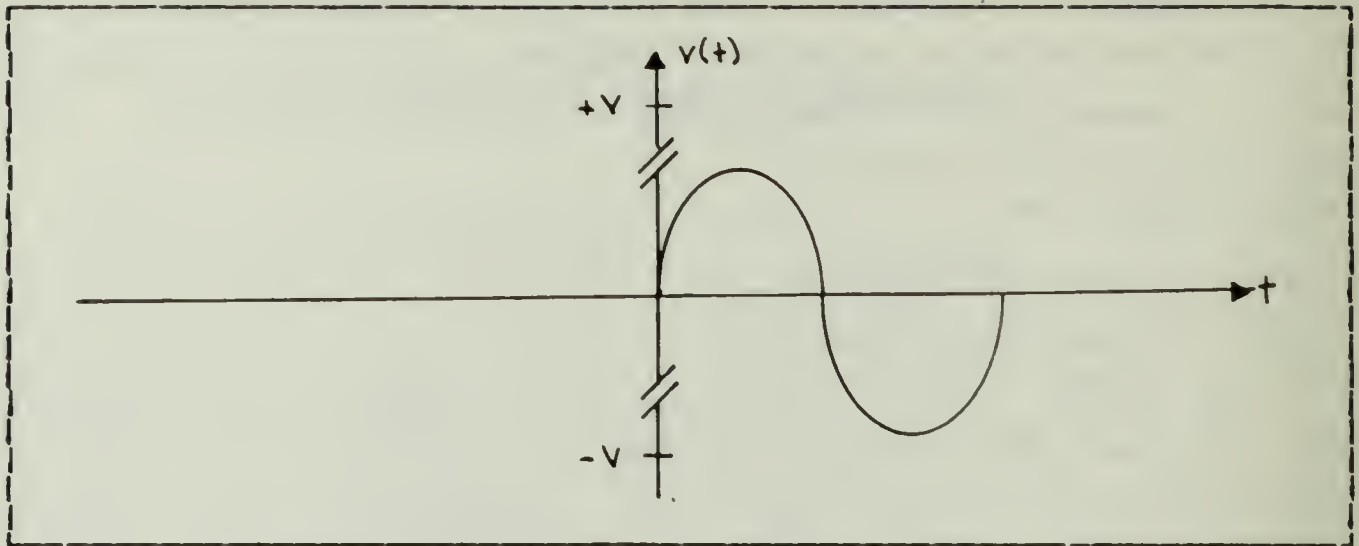


Figure 4.2 Analog Nature of Samples

$$\# \text{quantization levels} = 2^{*n} \quad (\text{eqn } 4.1)$$

for $n = 8$ bits/binary code word

$$\begin{aligned} \# \text{quantization levels} &= 2^{*8} \\ &= 256 \end{aligned}$$

place by determining into which quantization level the respective sample values fall and assigning that sample value the binary number associated with that quantization level.

Now each sample value is assigned to an eight bit binary code word. For voice transmission it has been shown that the minimum transmission rate was $T_s = 125$ microsec/sample. The bit rate is then simply equal to the number of bits per sample times the inverse of the transmission rate as illustrated in equations 4.2 and 4.3.

If voice was to be time multiplexed onto a single channel, the bit rate for that channel would be the number of signals per channel times the bit rate for the most time intensive signal as illustrated in equation 4.4.

$$\begin{aligned} \text{bit rate} &= (n \text{ bits/sample}) (1 \text{ sample}/T \text{ sec}) && \text{(eqn 4.2)} \\ \text{bit rate} &= (8 \text{ bits/sample}) (1 \text{ sample}/125 \text{ microsec}) \\ &= 64 \text{ kbps} \end{aligned}$$

$$\begin{aligned} \text{bit duration} &= 1/\text{bit rate} && \text{(eqn 4.3)} \\ &= 1/64 \text{ kbps} = 15.6 \text{ microsec/bit} \end{aligned}$$

$$\begin{aligned} (\# \text{signals/channel}) (\text{bit rate/signal}) &= && \text{(eqn 4.4)} \\ \text{bit rate/channel} & && \end{aligned}$$

In other words, if 24 voice signals are to be multiplexed onto a single channel, the bit rate must be

$$\begin{aligned} \text{bit rate/channel} &\geq && \text{(eqn 4.5)} \\ (24 \text{ signals/channel}) (64 \text{ kbps/signal}) \\ &= 1536 \text{ Mbps} \end{aligned}$$

As can be seen, the data transmission rate increases significantly, necessitating better and better hardware and a wider and wider bandwidth. Advantages should be readily apparent for A to D conversion techniques or modulation techniques that reduce the bit rate required.

Recovery of the analog signal is by a process called Digital to Analog Conversion. All that will be said about D to A conversion is that it is the inverse process of A to D conversion and that a slight error is always introduced during the process due to the discrete nature of the quantization process during A to D and D to A conversion.

B. DIFFERENTIAL PULSE CODE MODULATION (DPCM)

In DPCM, what is converted to binary numbers is not the quantization level (decimal number) which each sample value

is represented by but the successive differences between quantization levels. The idea is that the range of maximum difference values will be smaller than the range of actual sample values. It is therefore possible to represent that range of delta values with fewer bits/binary word and therefore fewer quantization levels and ultimately a lower bit rate. [Ref. 11]

In actual practice, in a DPCM conversion technique, it is a statistical estimate of each successive sample value which is subtracted from the actual value that is converted to binary code words. The result is the same in that the range of amplitudes is reduced and therefore fewer bits/word are required to represent the sample thereby lowering the data transmission rate required to transmit the signal. [Ref. 11]

C. DELTA MODULATION (DM)

Delta modulation is a form of DPCM where successive quantization levels of the output differ by only 1 bit. That is to say that any successive quantization level can be represented by varying only one bit of successive output binary code words. In other words a type of gray code is employed. This A to D technique is implemented through the use of a DM coder or linear delta modulator. This DM coder approximates a given input signal with a series of linear segments of uniform slope. A comparison is made between the value of this approximation and the input signal at each sample increment. The sign of this difference value is what is encoded and is used to increment the DM coder in the direction of the input signal. By using the differential sign value of the input signal and the incremented approximation from the DM coder the linear approximation from the linear delta modulator is said to "track" the input

signal. [Ref. 8] Slope overload of this type of modulation technique occurs when the slope of the incoming signal exceeds the ability of the DM system to follow the source at the sampling rate being utilized. [Ref. 11].

V. DIGITAL SIGNAL MODULATION TECHNIQUES

Digital signal modulation techniques are the methods of encoding information for transmission utilizing digital technology. Factors affecting digital modulation include, but are not limited to, the physics of the method, hardware requirements, bandwidth considerations, power requirements, data transmission rates and error probabilities. It is these aspects which will be explored in the following sections.

A. DIGITAL MODULATION FORMATS

Modulation is the technique by which the characteristics of one waveform (called the carrier) are varied or modified by the characteristics of another (called the source). The carrier waveform of interest is the sinusoid. It should be obvious that the attributes of a particular sinusoid that differentiate it from every other sinusoid are its amplitude, phase and frequency. It follows that the characteristics of the carrier waveform to be varied by the source are its amplitude, phase, frequency or any combination of the three. This gives rise to the broad general formats of Amplitude Shift Keying (ASK), Phase Shift Keying (PSK) and Frequency Shift Keying (FSK). All other digital modulation techniques are variations of or combinations of these basic formats. Other factors involved in the description of the digital modulation technique being employed include the number of bits being encoded at one time, the employment of error correction techniques and the baseband (source) waveform.

When each bit of the baseband waveform is individually encoded by any of the techniques previously mentioned (ASK, PSK, FSK), the technique being utilized is referred to as binary encoding. When more than 1 bit of the source code is modulated onto the carrier at one time it is called block encoding. Block encoding allows for one of $m = 2^k$ waveforms where $k =$ number of bits.

This paper will not go deeply into signal detection or demodulation techniques, however, a basic understanding of what is involved is necessary and again further defines the digital modulation format being employed. In general terms, signal detection is referred to as either coherent or noncoherent detection of the transmitted signal. Coherent detection, perhaps the easiest to understand, is when all possible waveforms of the modulated carrier waveform are available at the receiver and the waveform at the receiver is in phase with the transmitted carrier. Noncoherent detection is involved when the receiver does not have knowledge of the phase of the transmitted information and one of a number of phase estimation techniques must be employed for signal recovery.

B. HARDWARE

Although significant advances have been made in recent years to improve the quality of hardware associated with satellite communications, most components are not what would be considered "off the shelf items". The hardware components most commonly referred to with regard to digital communications include the sampler, encoder, modulator, multiplexer and transmitter. There are variations of the above hardware requirements necessary for certain types of digital formatting, however, those exceptions will be addressed separately when the individual modulation techniques are examined.

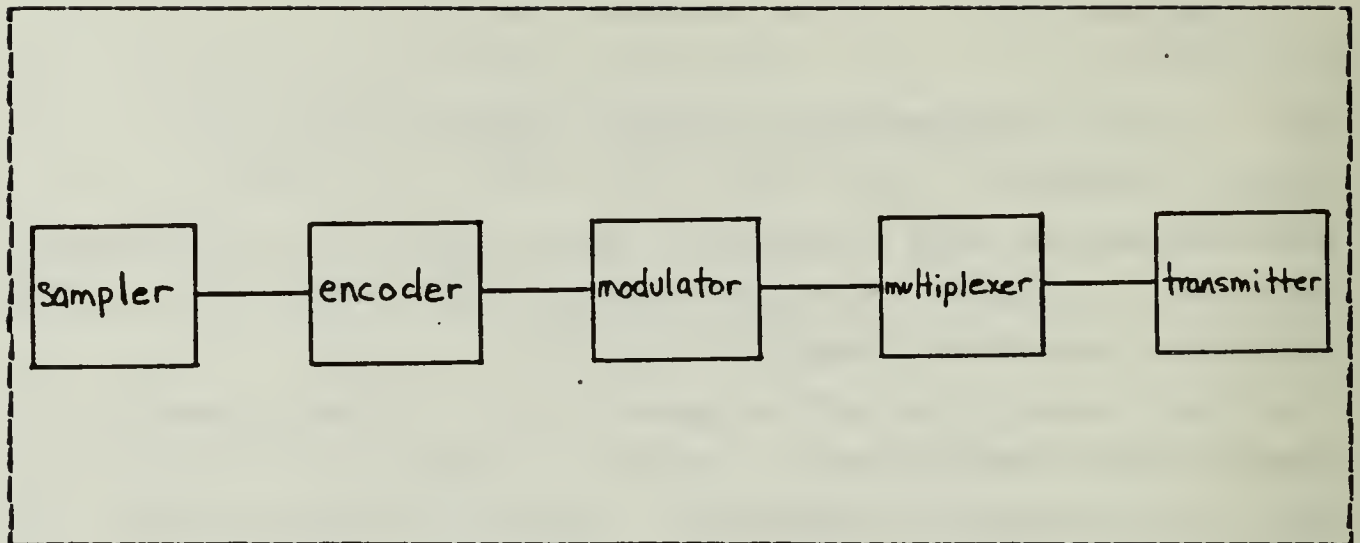


Figure 5.1 Basic Hardware Component Block Diagram

1. Sampler

The sampler is the device or component which samples or extracts those single characteristic values of a naturally occurring analog signal which are ultimately encoded into a digital word by the encoder. The frequency at which this sampler must operate was derived in the discussion of the Sampling Theorem. It was determined that the sampler must operate at a frequency greater than 2 times the highest significant Fourier frequency component of the source voltage. Modern solid state devices capable of taking thousands of samples/sec are available at modest costs.

2. Encoder

Often referred to as the A to D converter (analog to digital converter), the encoder transforms the samples of the analog signal derived from the sampler into a digital format through one of the analog to digital conversion techniques described in the chapter on A to D conversion. These digital bits can be stored for later use, coded,

delayed or used immediately either individually or in groups to modify one of the characteristic qualities of the carrier waveform. When sample values of the analog source signal are converted into digital bits of information, they are simply that, digital bits of information. The carrier can only be modified to represent the source information by interaction with another voltage. Therefore the value of the digital bit (binary), either 0 or 1, is used to generate a baseband waveform or voltage which does the actual modulation of the carrier waveform.

a. Common Baseband Waveforms

It should be obvious that since it is desired to represent binary code words with a representative baseband waveform what is required is two levels of voltage. There are two basic logic schemes for representation of the baseband waveform. They are bipolar or unipolar logic. Bipolar logic involves representing the 0's or 1's of the binary codeword as either $+V$ or $-V$ as illustrated in Figure 5.2.

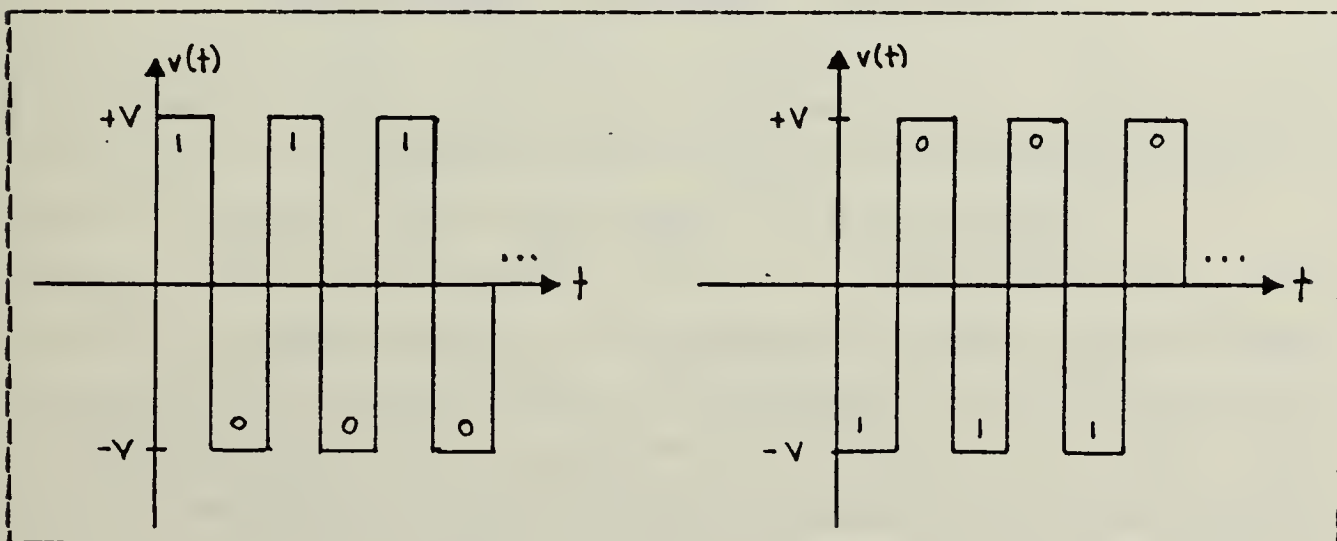


Figure 5.2 Bipolar Logic

The 0 or the 1 of the binary code word can be represented either as $+V$, $-V$ or $-V$, $+V$ respectively. This is a matter of convention but must be clearly understood in the various component designs in order to ensure compatibility between parts of the system.

Unipolar logic utilizes a voltage to represent either of the possible binary digits and the absence of voltage to represent the other. Two common conventions of unipolar logic are represented in Figures 5.3 and 5.4.

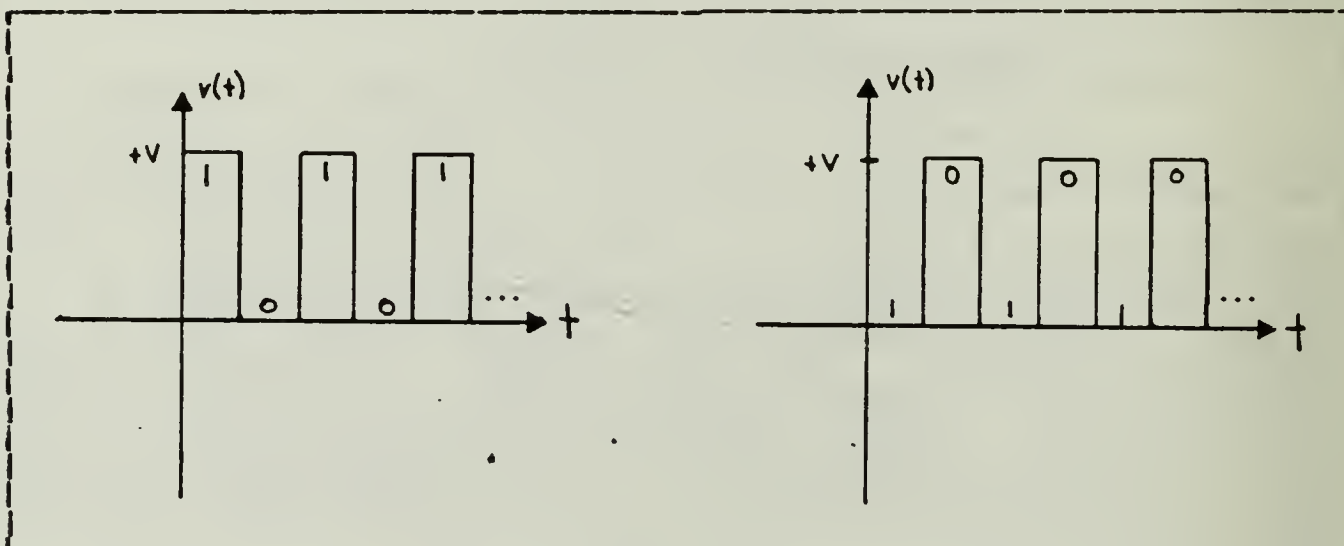


Figure 5.3 Unipolar Positive Logic

Again, which form of unipolar logic might be employed in the A to D converter is a matter of convention.

Variations of these two basic encoding formats have the advantages of ease of generation and improved decoding and clock recoverability. Two variations commonly used in satellite communications are the Non Return to Zero (NRZ) and the Manchester waveforms. The NRZ waveform is simply the voltage representation which corresponds to the stream of bits represented in the logic scheme chosen. There is no transition as long as the same bit is present. Choosing bipolar logic as an example, a NRZ waveform can be described schematically as in Figure 5.5.

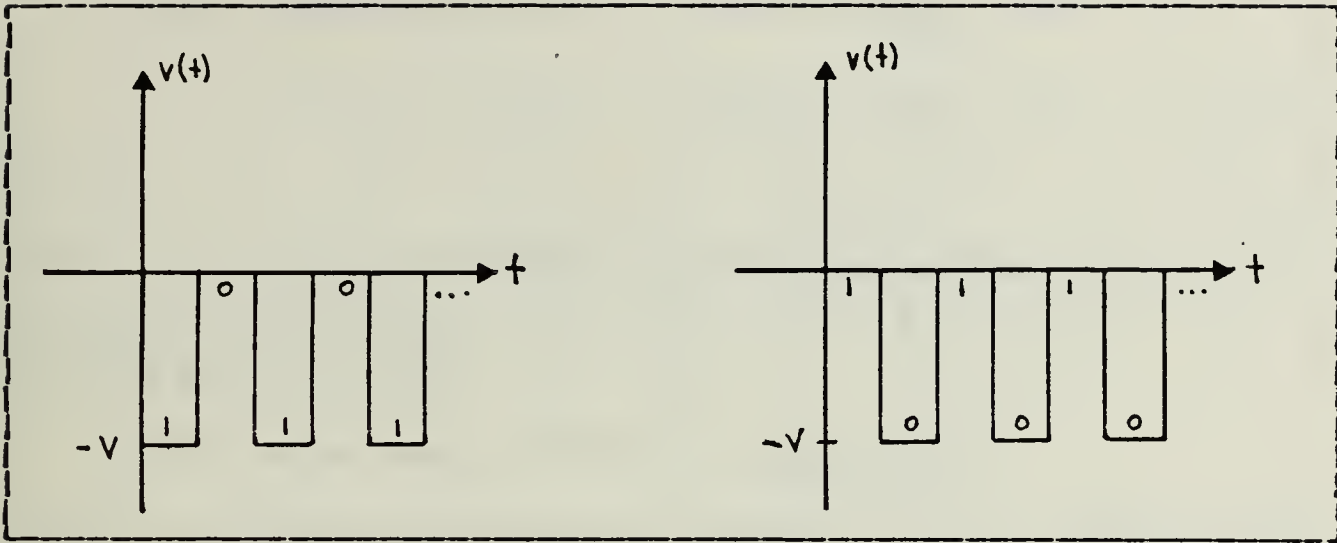


Figure 5.4 Unipolar Negative Logic

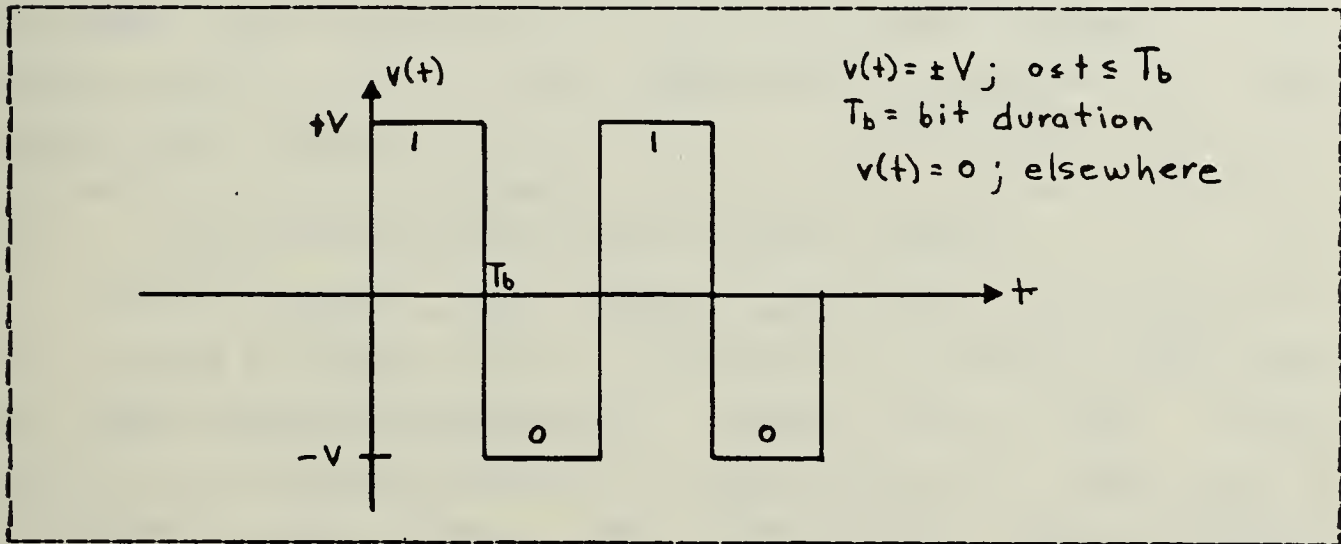


Figure 5.5 Non Return to Zero Waveform

The Manchester waveform of the same source voltage is represented with a transition at the midpoint of the bit duration from either $+V$ to $-V$ or $-V$ to $+V$. This form of coding has the advantage of clock synchronization in all cases of digital encoding. Schematically, the Manchester code can be represented as in Figure 5.6.

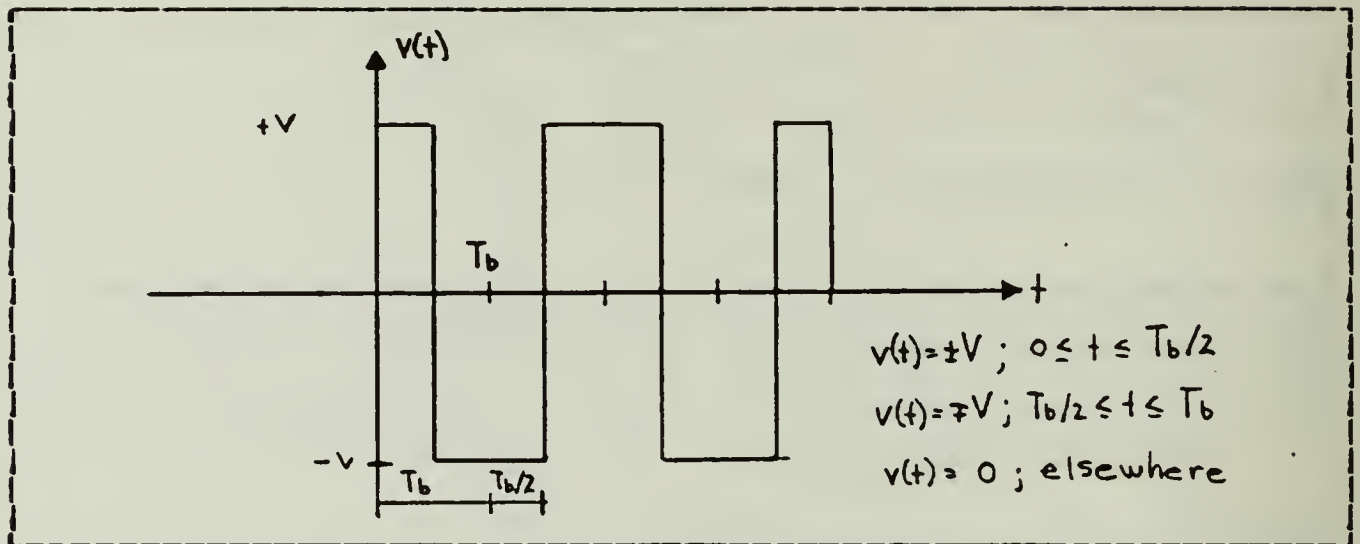


Figure 5.6 Manchester Waveform

3. Modulator

The modulator in a digital communications system is more commonly referred to as a modem (modulator/demodulator). This device does the actual transformation of the digital information into a waveform that can be transmitted from one point to another. The modulation as mentioned earlier can modify either the amplitude, phase or frequency of the carrier wave. In simple terms, the digital information derived from the analog source is mapped into the carrier wave. It is this mapping that determines the power and bandwidth characteristics of the modem.

4. Multiplexer

Multiplexing is a common method for increasing the utility of a given communications channel. Variations in multiplexing techniques give rise to the multiple access techniques employed in satellite communications.

a. Frequency-Division Multiplexing (FDM)

Frequency-Division Multiplexing is a technique whereby the capacity of a communications channel is increased by adding one signal to another. These signals occupy discrete nonoverlapping frequency bands. A specific signal is recovered by use of a band pass filter for the frequency band desired. [Ref. 7]

b. Time-Division Multiplexing (TDM)

Time-Division Multiplexing is a technique used to increase the capacity of a given communication channel by adding signals in time. That is, specific signals or portions of signals are allocated specific time slots or portions of the carrier wave. These time allocations cannot overlap and the signal is recovered through proper synchronization of the recovery hardware with the multiplexer. [Ref. 7]

c. Code-Division Multiplexing (CDM)

Code-Division Multiplexing is a technique for increasing the capacity of a given communications channel through the assignment of a characteristic code to the digital signal before it is multiplexed in the time or frequency domain. Since the code used in multiplexing is known at the demultiplexer, recovery of the digital source code could be accomplished through the use of a matched filter or correlator. [Ref. 7]

C. BANDWIDTH

For purposes of discussion and for uniformity, when examining the various digital signal modulation techniques of interest, the bandwidth will be defined as the highest significant Fourier frequency component of the signal in

question. For digital communications, it can be shown that by the above definition, the bandwidth of the baseband waveform is $1/T_b$, where T_b is the bit duration. For example:

1. Voice sampled at the rate of 8000 samples/sec
2. Each sample represented by an 8 bit code word
3. $R_b = \text{bit rate} = (8000 \text{ samples/sec}) (8 \text{ bits/sample})$
 $R_b = 64 \text{ kbps}$
4. $T_b = \text{bit duration} = 1/R_b$
 $T_b = 15.6 \text{ microsec}$

The Fourier transform of the baseband waveform of duration 15.6 microsec is represented in Figure 5.7.

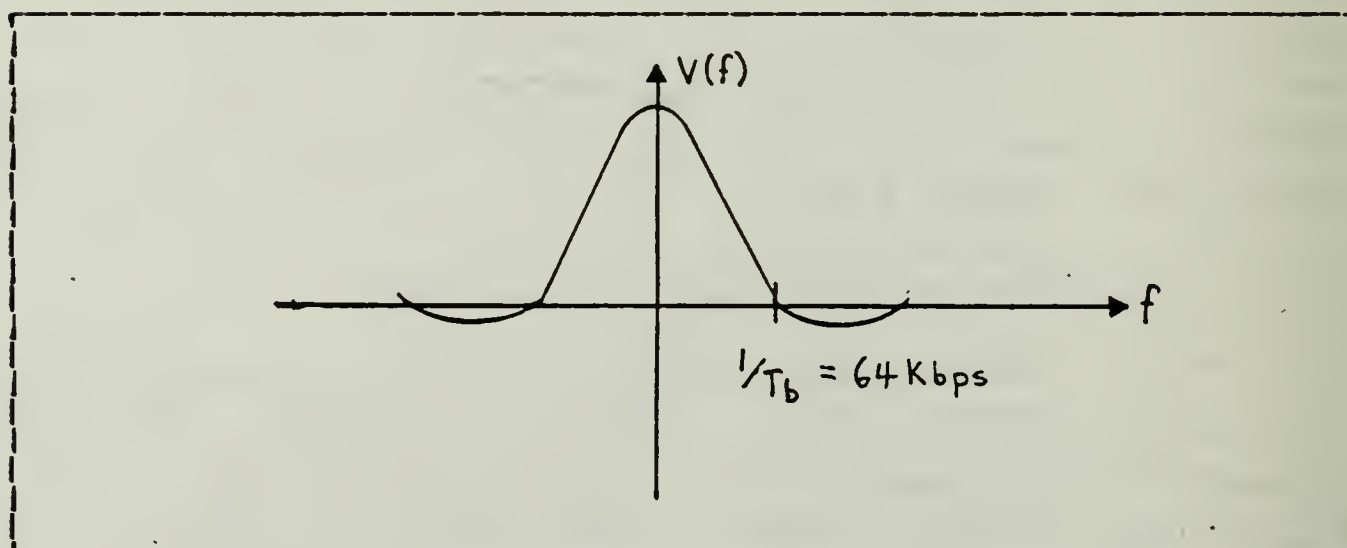


Figure 5.7 Fourier Transform of Baseband Waveform

It should be readily apparent that as the bit rate of the digital baseband waveform increases, so does the bandwidth. It is desirable to keep the bandwidth of the signal to a minimum due to limitations on availability of the electromagnetic spectrum. In addition, interference with signals which occupy adjacent frequency bands is reduced and propagation limitations of the medium and hardware limitations such as self-inductance and capacitance are minimized.

D. SPECIFIC TECHNIQUES

Now with some of the basics of digital signals already introduced it is possible to investigate some of the more significant modulation formats employed in digital satellite communications. The organization of this section will be around the three general types of modulation, i.e., phase, amplitude and frequency. Within each broad category, several techniques will be described under the subareas of binary encoding, where the information is modulated onto the carrier bit by bit, and block encoding, where groups of bits do the modulation. Variations of these areas will be pointed out. The characteristics of the modulation technique will be introduced including, where practical, an analytical description, phasor representation, error probability, spectral efficiency, advantages and disadvantages.

1. Phase Shift Keying (PSK)

Phase shift keying is a generic form of signal modulation where the baseband waveform is used to modify or change the phase of the carrier. Phase, as stated earlier is one of the characteristics which distinguish one sinusoid from another. In general, phase shift keying offers the advantages of power and bandwidth efficiency.

a. Binary Phase Shift Keying (BPSK)

As the name suggests, Binary Phase Shift Keying (BPSK) results in a modulated carrier waveform consisting of two phases of the same sinusoid. The baseband waveform is used to change the phase of the carrier bit by bit from one phase to the other. In the case of bipolar logic, the bit stream consists of ± 1 . The general waveform of the carrier can be represented as a cosine wave of amplitude A , angular

frequency ω and initial phase angle δ as in equation 5.1.

$$v_c(t) = A \cos(\omega t + \delta) \quad (\text{eqn 5.1})$$

Since two phases are represented in $v_c(t)$, it is customary to let them differ by π radians. This can be represented by the modification of equation 5.1 to account for a π phase shift depending on whether the bit, $v(t)$ to be modulated is either a $+1$ or -1 as shown in equation 5.2.

$$v_c(t) = A \cos(\omega t + \delta + \pi/2(1-v(t))) \quad (\text{eqn 5.2})$$

Equation 5.2 can be expanded to result in a simplified form showing that the modulated carrier waveform is simply a product of the baseband waveform and the carrier. See equation 5.3 where $v(t)$ represents the baseband waveform.

$$v_c(t) = A v(t) \cos(\omega t + \delta) \quad (\text{eqn 5.3})$$

A phasor diagram can be constructed to represent the modulated carrier waveform in BPSK and is shown in Figure 5.8. As can be seen by the phasor diagram in Figure 5.8, the phase of the modulated waveform depends on the value of the baseband waveform and differs by π depending on whether the value of the modulated bit is ± 1 .

Remembering the section on the properties of the Fourier transform, it is possible to analyze the spectral and power efficiency of BPSK. Recall BPSK can be created by multiplication. Multiplication of two voltages is covered by the frequency translation property of the Fourier transform. Frequency translation results in double the bandwidth or spectral requirement of the translated waveform and half the power. In the case of a NRZ baseband waveform,

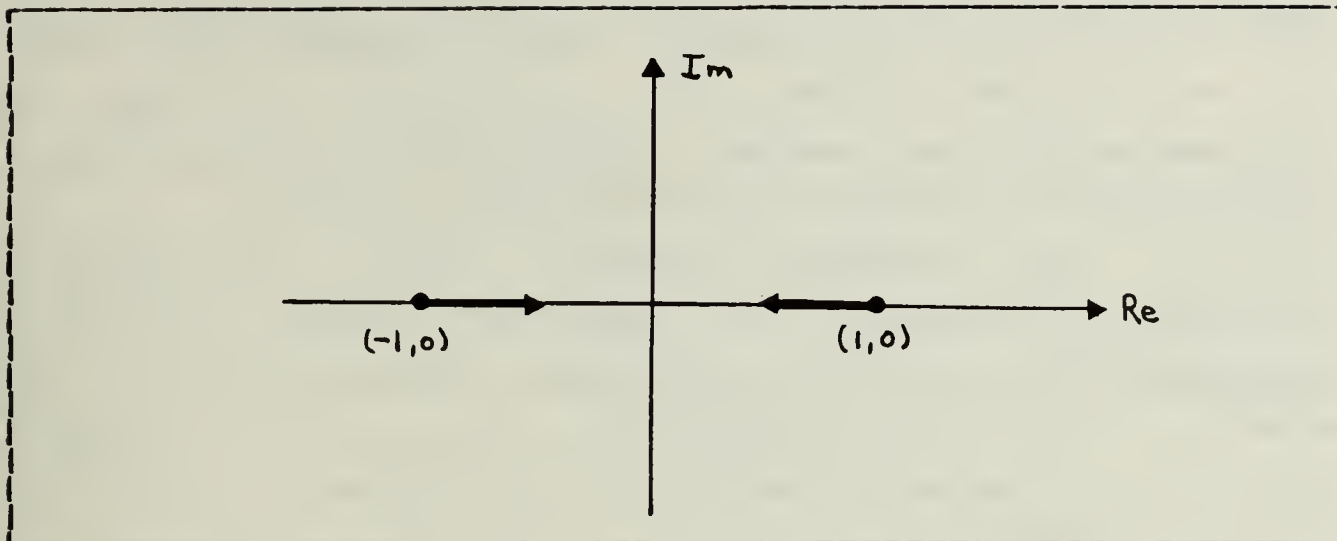


Figure 5.8 Phasor Diagram of BPSK

the bandwidth of the non-translated pulse, determined from the largest significant Fourier frequency component is $1/T_b$, where T_b is the bit duration. The bandwidth of the translated voltage (BPSK carrier) is $2/T_b$. The power in a sinusoid is $A^2/2$ and none of this power capacity is lost in BPSK since only the phase of the original sinusoid is changed. For a Manchester baseband waveform, the non-translated signal has bandwidth $2/T_b$ and the translated wave has bandwidth $4/T_b$.

The advantage of BPSK is that it is relatively efficient in bandwidth utilization and power capacity. It does have the disadvantage of fairly large sidelobe components which contribute to interference with adjacent frequencies. This usually necessitates some type of filtering before the signal can be transmitted.

b. Differential Binary Phase Shift Keying (DBPSK)

The recovery of a Binary Phase Shift Keyed signal requires the use of a phase coherent reference signal as described in the previous sections on autocorrelation and matched filters. This may not always be practical or

possible so a technique called Differential Binary Phase Shift Keying has been developed. DBPSK uses the same carrier type as BPSK and offers many of the same advantages and disadvantages. As stated, the primary difference is the lack of necessity for a phase coherent reference.

The baseband waveform, $v(t)$, for DBPSK is generated by comparing the phase of the next bit to be transmitted to that of the previously transmitted bit. For example, if a +1 is encoded onto the carrier as $v(t)$, it represents a particular phase of the carrier. If the next bit to be sent is also a +1, there is no phase change, i.e., the bit remains the same over two successive bit durations. If, however, the second bit to be sent is a -1, this represents a π phase change and is decoded as a bit change over successive bit durations. This can be expressed mathematically as in equation 5.4 where b_k represents the bit which will be encoded on the carrier and b_{k-1} represents the previous bit already encoded and a_k represents the present bit.

$$b_k = b_{k-1} \cdot a_k \quad (\text{eqn 5.4})$$

As can be seen when $b_k = -1$, there is a phase change and the bit changes from one bit to the next depending on the logic type being employed. If $b_k = +1$, this represents the phase remaining constant over two successive bit durations, i.e., no bit change. See Figure 5.9 [Ref. 8]. Recovery is effected by correlation of the received bit to the previously received bit.

Differential Binary Phase Shift Keying (DBPSK) differs from Differentially Encoded Binary Phase Shift Keying (DEBPSK) in the recovery step only. DBPSK takes advantage of the modulation of phase shift in the recovery process while DEBPSK still utilizes a phase coherent carrier

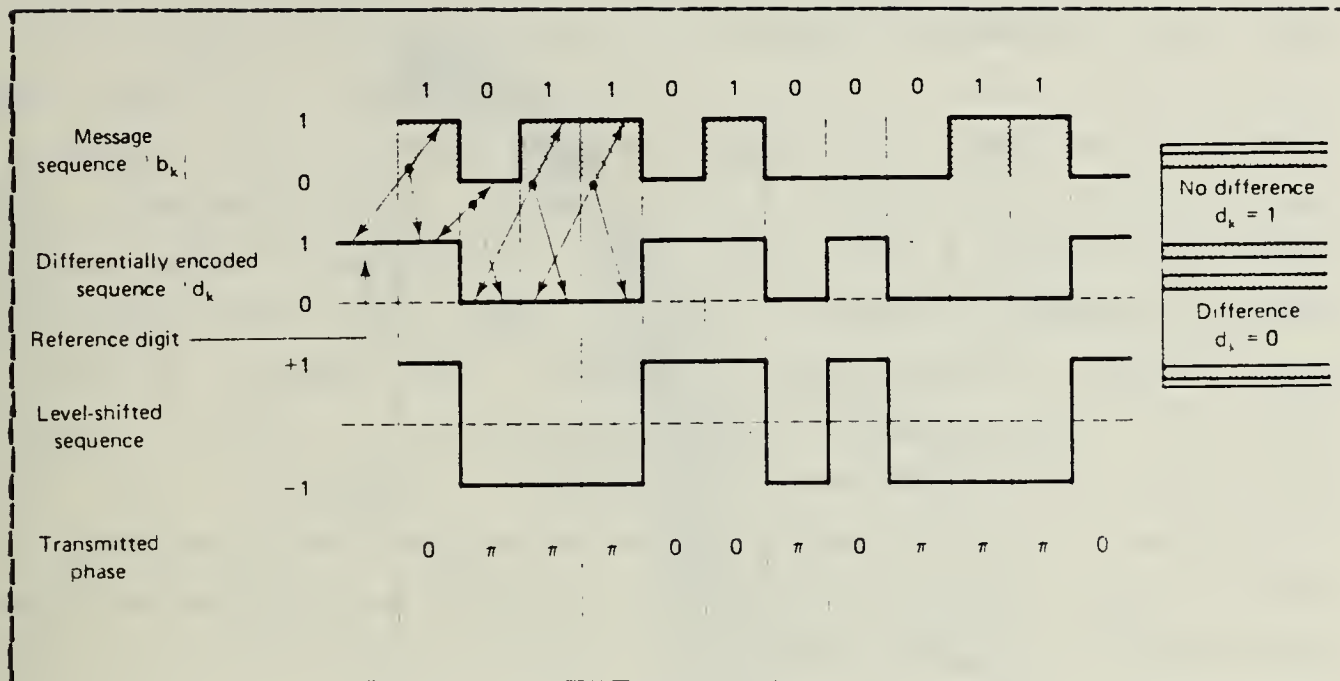


Figure 5.9 Differential Binary Phase Shift Keying

signal in demodulation. Both cases use the same scheme for differential encoding.

c. Orthogonal Binary Phase Shift Keying (Orthogonal BPSK)

In Binary Phase Shift Keying there is always a probability, with the interjection of noise on the transmitted signal that an individual bit will be decoded incorrectly from that which was actually transmitted. In some environments, this probability is so high that special encoding techniques must be employed in order to reduce the probability that a bit or a binary code word will be decoded in error. One such technique is Orthogonal BPSK. Orthogonal BPSK is a type of group encoding scheme where groups or blocks of bits from the original signal are assigned redundant bits according to a predetermined assignment routine. This new expanded sequence of bits is then transmitted as before in BPSK.

For example, assume that it has been determined that the respective values of the original signal will be represented by a k bit binary code word. It has been demonstrated that there exists 2^{**k} binary code words, k bits long in this type of arrangement. With Orthogonal BPSK there also exists 2^{**k} orthogonal sequences of bits (called channel symbols, bauds or chips) [Ref. 6], which represent the k binary code words. However, the number of bits or chips in the sequence is increased to $n = 2^{**k}$, thereby providing the desired redundancy. Each of the 2^{**k} sequences of n chips is constructed to be orthogonal to every other sequence in order to assure maximum separation. See Figure 5.10 [Ref. 6].

$k = 2$ data word	Orthogonal chip sequence		Transmitted waveforms
			BPSK carriers with phase shifts below:
1 1	1 1 1 1	$C_1(t)$	$\pi \quad \pi \quad \pi \quad \pi$
1 0	1 -1 -1 -1	$C_2(t)$	$\pi \quad \pi \quad -\pi \quad -\pi$
0 1	1 -1 -1 1	$C_3(t)$	$\pi \quad -\pi \quad -\pi \quad \pi$
0 0	1 -1 1 -1	$C_4(t)$	$\pi \quad -\pi \quad \pi \quad -\pi$
			$\leftarrow T \rightarrow$ $\leftarrow T_w \rightarrow$

Figure 5.10 Orthogonal Binary Phase Shift Keying

Decoding is also done by blocks through a bank or 2^{**k} correlators. Since the decoding is done in blocks, the probability that the entire transmitted code word will be incorrectly decoded is reduced even though individual bits are incorrectly decoded. This is the major advantage of Orthogonal BPSK. Figure 5.11 [Ref. 6], shows the reduction in error probability with Orthogonal BPSK

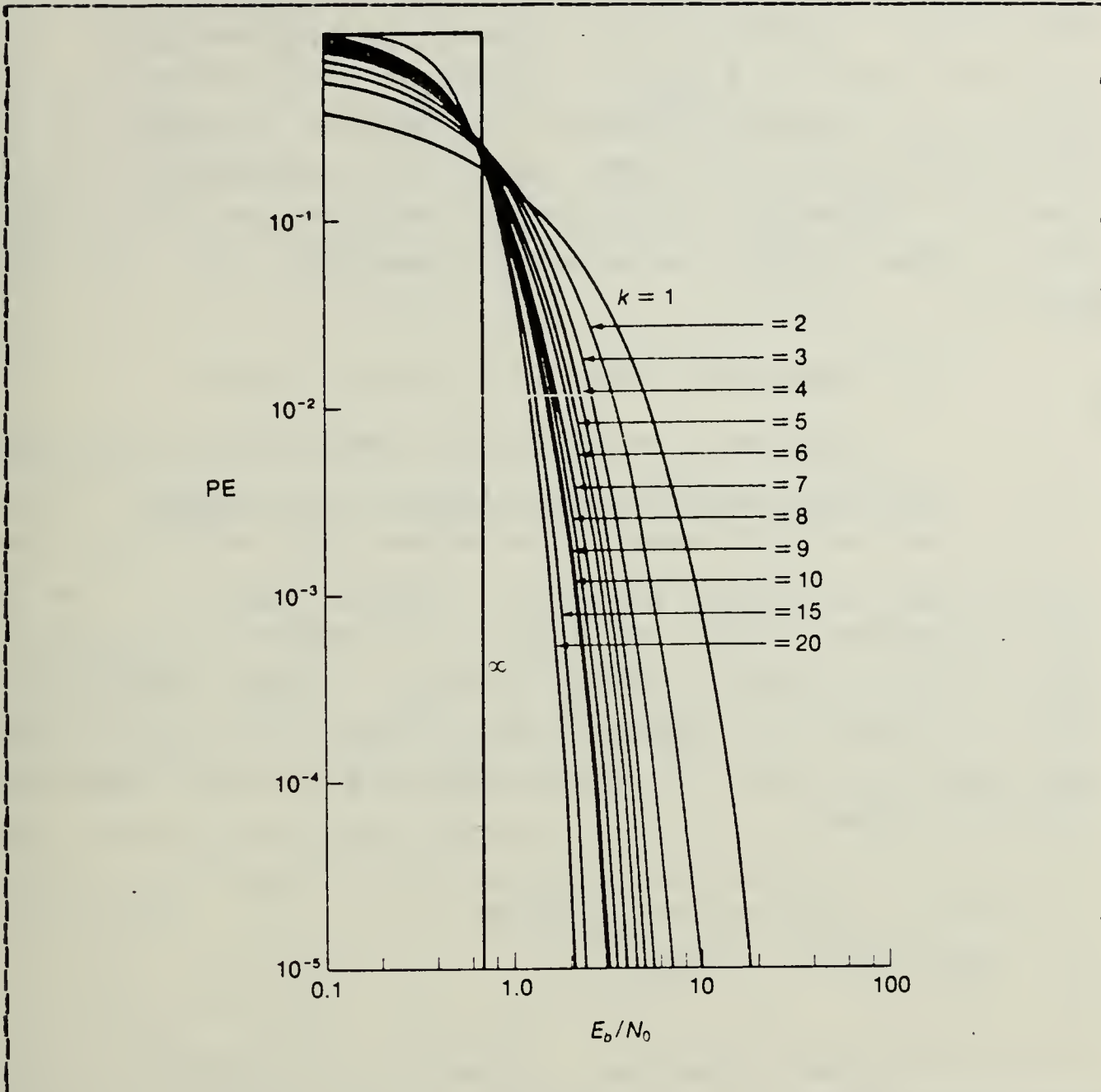


Figure 5.11 Probability of Error for Orthogonal BPSK

The major disadvantage to Orthogonal BPSK is that it results in a reduced data bit rate at a given transmission rate or the necessity for a higher transmission rate if the same bit rate is to be maintained. For example, suppose the bit rate of a PSK signal is R bits/sec. If each of the k bits in the PSK signal are represented by $2 \cdot k$ chips as is the case in Orthogonal BPSK modulation, then the

bit rate must be $(2^{**k}/k)R$ if the same data rate is to be maintained. Additionally, since the necessary bit rate increases, the bit duration decreases. It was shown in the section on bandwidth that as bit duration decreases as the result of a higher bit rate, an increase in bandwidth is the result. Therefore, the tradeoff in decreased transmission error comes at the expense of bandwidth and bit rate. [Ref. 6]

d. Quadrature Phase Shift Keying (QPSK)

Quadrature Phase Shift Keying derives its name from a four-phase modulation of the carrier waveform. These modulations are achieved by simultaneously modulating the inputs from two bit streams onto a single carrier. The two bit sequences could be from two separate sources or successive bits from a single source. To take advantage of the orthogonality of the sine and cosine functions, QPSK can be viewed as in equation 5.5 as the sum of a BPSK modulated sine and cosine.

$$v_c(t) = A v_1(t) \cos(\omega t + \delta) + A v_2(t) \sin(\omega t + \delta) \quad (\text{eqn 5.5})$$

The signal can also be represented as in equation 5.6 where the phase angle, θ , of the modulated carrier is shown in equation 5.7.

$$v_c(t) = 2^{*.5} A \cos(\omega t + \theta + \delta) \quad (\text{eqn 5.6})$$

$$\theta = \arctan (v_1(t)/v_2(t)) \quad (\text{eqn 5.7})$$

The phases possible as a result of substitution of the possible bits in bipolar logic in equation 5.7 are ± 45 degrees and ± 135 degrees. See Figure 5.12.

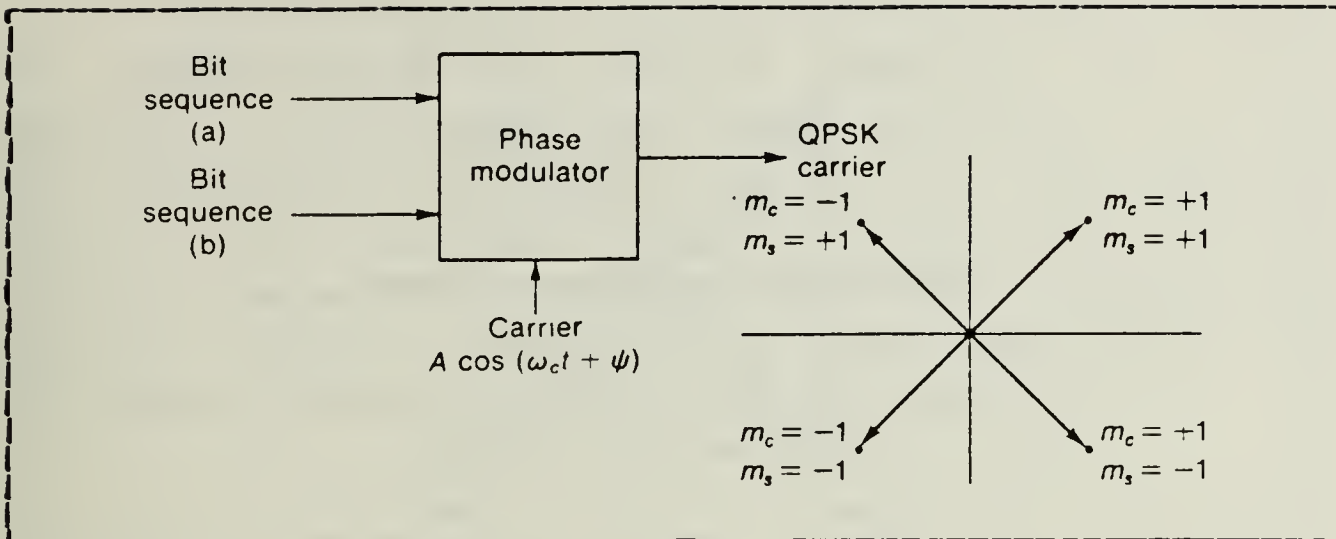


Figure 5.12 Modulation and Phases of QPSK

Since two bits are being encoded at one time for transmission, the bit rate in QPSK is twice that of BPSK. The BPSK bit rate is equal to the QPSK symbol rate, (symbol rate being the time the quadrature bits exist on the carrier). It is the symbol rate in QPSK which determines the bandwidth and since symbol rate is equal to bit rate in BPSK, the bandwidth of the two modulation techniques is identical. The great advantage of QPSK lies in the bandwidth utilization. Two bits of information are transmitted thereby effectively doubling the bit rate at no additional cost in bandwidth. A phasor representation of QPSK is illustrated in Figure 5.13. Each quadrature component of the modulated signal contains half the power of the total carrier or $(A^2/2)/2 = A^2/4$.

e. Offset Quadrature Phase Shift Keying (OQPSK)

In Quadrature Phase Shift Keying, both bits of the two baseband waveforms, which are to be modulated onto the carrier, change at the beginning of the respective symbol time. This allows the phase of the carrier to change up to 180 degrees for each symbol as illustrated in the

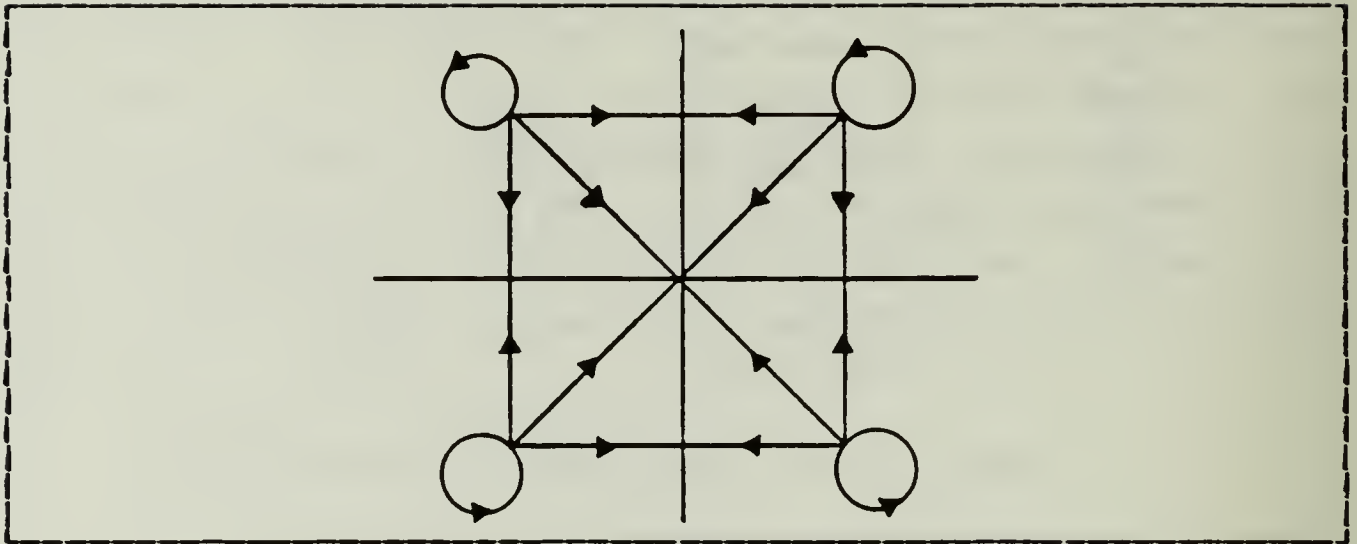


Figure 5.13 Phasor Diagram of QPSK

phasor diagram in Figure 5.13. The phase change of the modulated signal can be limited to 90 degrees through a modulation technique called Offset Quadrature Phase Shift Keying. This is accomplished by delaying the application of the second baseband channel for $T_s/2$ seconds, where T_s is symbol duration as illustrated in Figure 5.14. Modulation is then accomplished as before in QPSK.

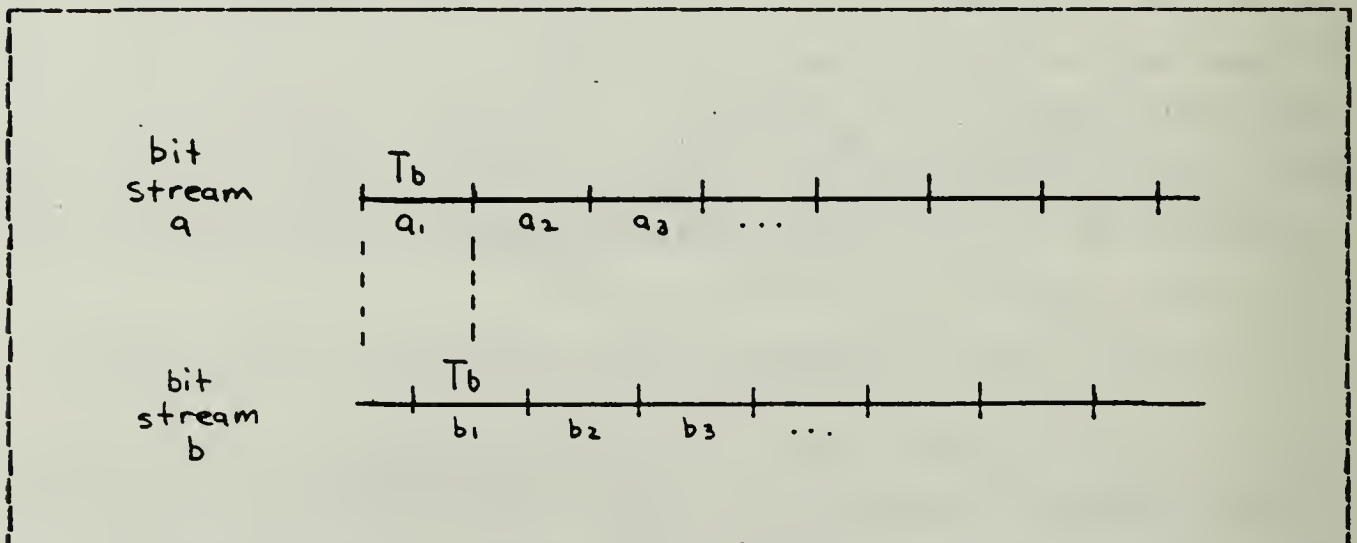


Figure 5.14 Offset Quadrature Phase Shift Keying

The result is a QPSK modulated signal in which the maximum phase shift between successive bits is 90 degrees. The bandwidth and power spectra of an OQPSK modulated signal are the same as that of a QPSK modulated signal. The advantage of OQPSK is in the limit which is placed on phase shift during encoding which simplifies the encoding hardware. Additionally OQPSK has spectral and interference advantages during decoding [Ref. 6].

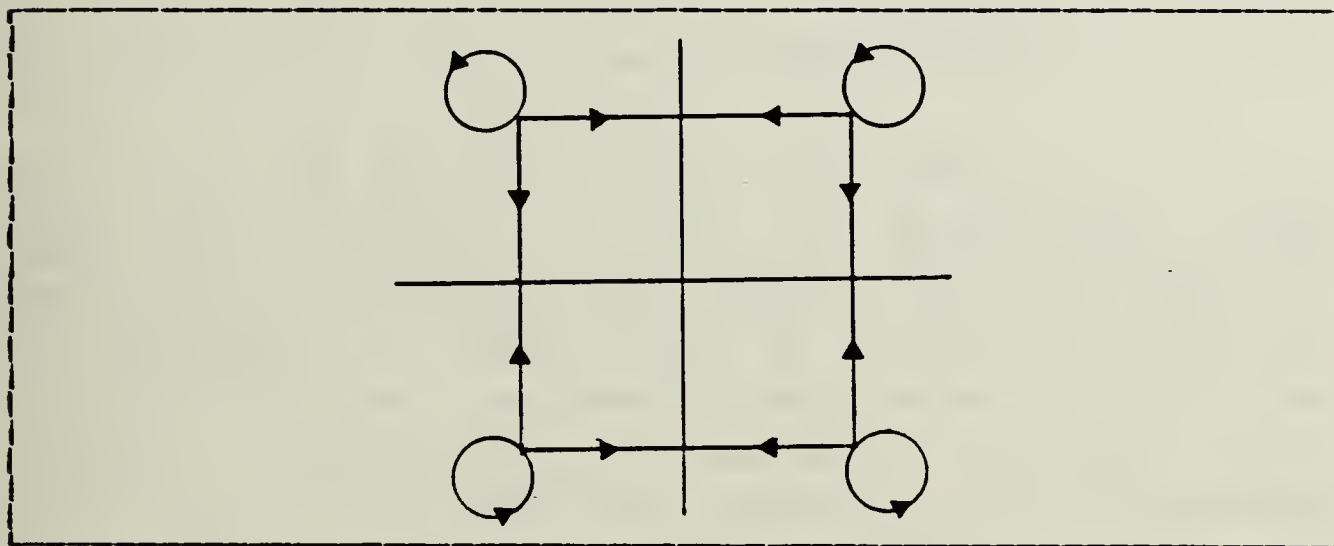


Figure 5.15 Phasor Diagram of OQPSK

f. Multiple Phase Shift Keying (MPSK)

Another form of digital modulation is known as Multiple or M-ary Phase Shift Keying (MPSK). Once again, as in Orthogonal Binary Phase Shift Keying, k data bits are transmitted. The k bits represent the word length and there are $m = 2^k$ different binary words, k bits long, for this type of modulation. In MPSK, the binary code word is used to vary the phase of the carrier. There are therefore $m = 2^k$ different phases in MPSK. These sequences of binary digits need not be orthogonal as in Orthogonal Binary Phase

Shift Keying. The length of the transmitted symbol is only k bits long as compared to 2^k bits for Orthogonal BPSK. The phases therefore are not all orthogonal leading to greater difficulty in decoding and a higher probability that an individual code word will be incorrectly decoded, especially as m becomes large.

As in other types of Phase Shift Keying, MPSK can be represented as in equation 5.8 where $\theta = \text{phase} = (2\pi/m) i; i=0, 1, \dots, m-1$.

$$v_c(t) = A \cos(\omega t + \theta + \delta) \quad (\text{eqn 5.8})$$

An advantage of MPSK is that as long as the symbol transmission rate does not increase, the carrier bandwidth does not increase even as the size of the binary code word increases. The disadvantage, as stated earlier, has to do with error rates in decoding. Decoding requires a phase coherent reference of considerable stability especially as m increases and respective phases become closer together. Practical limits for this type of modulation is $m = 8$ or a 3 bit binary code word due to the complexity of the encoding and decoding hardware.

2. Amplitude Shift Keying (ASK)

Amplitude Shift Keying, as the name implies is modulation of the carrier through variation of its amplitude due to variations in the baseband waveform. The information in the baseband waveform is thereby imparted to the carrier through this modulation. Since the amplitude of the carrier varies between successive symbols or binary code words, the power also varies. Recovery is by comparison of the transmitted power during each symbol to the possible $m = 2^k$ power levels.

a. Multiple Amplitude Shift Keying (MASK)

MASK is a type of group encoding where k bits are combined into a single waveform for transmission and subsequent recovery. Since each symbol or binary code word contains k bits, there are $m = 2^{**k}$ different symbols and consequently m different amplitudes of the carrier possible during the symbol duration time. An assignment scheme which maps the binary code words into the m different amplitudes would be to simply space them $A_i = A/m_i$ volts apart, where A is the maximum amplitude and m_i represents the decimal equivalent of the binary code word from $i = 1$ to 2^{**k} .

The analytic form of a MASK waveform is represented in equation 5.9 where all the variables are the same as presented earlier except for A_i which is equal to one of i different amplitudes depending on the bit sequence to be transmitted.

$$v_c(t) = A_i \cos(\omega t + \delta) \quad (\text{eqn 5.9})$$

MASK is not very popular in satellite communications since it depends on a carrier of very stable amplitude. This is not generally practical under actual conditions. However, MASK does have the spectral advantage of a constant bandwidth of $2/T_s$, T_s equal to symbol duration, even as the binary code word increases in length.

b. Quadrature Amplitude Shift Keying (QASK)

Quadrature Amplitude Shift Keying (QASK) is a hybrid digital signal modulation technique. It represents separate amplitude modulation of the quadrature components of a common carrier. In that sense it is both ASK and PSK. Implementation of QASK involves simultaneous application of M -ary Amplitude Shift Keying to the quadratures. See

equation 5.10, where A1 and A2 are derived according to an assignment scheme as in MASK.

$$vc(t) = A1 \cos(\omega t + \delta) + A2 \sin(\omega t + \delta) \quad (\text{eqn 5.10})$$

By this method, the effective bit rate is doubled over that of ordinary MASK. In other words, QASK results in the same data rate as modulating 2k bits onto the carrier at the same time or during the same symbol duration with MASK. The advantage to QASK lies in the fact that this increase in bit rate comes at no further increase in bandwidth. The disadvantages associated with MASK are still present with an additional increase in the complexity of the decoding equipment. Decoding of QASK must be done in two steps. First the signal is recovered in phase through a phase-coherent correlator and then each amplitude modulated signal is recovered as before in MASK by comparison of the power levels of the received signal.

3. Frequency Shift Keying (FSK)

Frequency Shift Keying (FSK), is the generic term used to describe a number of digital signal modulation techniques which cause variations in the carrier frequency by interaction with the baseband waveform. Decoding is generally through measurement of the frequency of the received signal.

a. Minimum Shift Keying or Fast Frequency Shift Keying

Power requirement for the transmission or retransmission of a satellite signal is extremely important. It is desirable to limit power required to accurately

transmit a piece of information to the minimum possible consistent with allowable error rates. For this reason, detection of FSK signals is limited to coherent methods as power required increases significantly for non-coherent methods.

MSK or FFSK are identical and represent a modulation technique known as continuous phase FSK. They get their names from the fact that "fast" indicates more bits per second can be transmitted in a given bandwidth than ordinary BPSK and "minimum" refers to the minimum modulation index for which orthogonal signalling occurs [Ref. 7].

Analytically, FFSK can be expressed as in equation 5.11 and equation 5.12.

$$v_c(t) = A \cos((\omega_c + \Delta\omega)t) \quad (\text{eqn 5.11})$$

$$v_c(t) = A \cos(\pm\Delta\omega t) \cos(\omega_c t) - A \sin(\pm\Delta\omega t) \sin(\omega_c t) \quad (\text{eqn 5.12})$$

As is noted, FFSK can be envisioned as the summation of separately modulated in-phase and quadrature components of the carrier by the baseband waveform. The technique is similar to that used in OQPSK. The frequency variation in the carrier waveform is between $\omega_c + \Delta\omega$ and $\omega_c - \Delta\omega$. Maximum separation in phase of these two frequency components occurs at π as noted in equation 5.13, where T_b represents the bit or symbol duration.

$$(\omega_2 - \omega_1)T_b = \pi \quad (\text{eqn 5.13})$$

This can be converted to the modulation index mentioned above simply by converting to frequency as in equation 5.14.

$$h = (f_2 - f_1)T_b = .5$$

(eqn 5.14)

For FFSK, the frequency deviation or separation between frequencies of the transmitted carrier is exactly $1/2T_b$ and the deviation from the carrier frequency is $1/4T_b$. FFSK can therefore be rewritten from equation 5.12 as in equation 5.15 by substitution for $\Delta\omega = 2\pi(1/4T_b)$.

$$v_c(t) = A \cos(\pm\pi t/2T_b) \cos(2\pi f_c t) - A \sin(\pm\pi t/2T_b) \sin(2\pi f_c t) \quad \text{(eqn 5.15)}$$

The error rate in this modulation technique is identical to that of BPSK. Frequency Shift Keying can be implemented to incorporate any given modulation index by simple calculation of the frequency separation with equation 5.14 and substitution into equation 5.15. For M-ary Frequency Shift Keying, the separation between frequencies must be at least $1/T_s$, where T_s is the symbol duration, in order to avoid carrier energy from one frequency being incorrectly interpreted as carrier energy from another frequency. This results in a modulation index of 1. Figure 5.16 represents the phasor diagram of an FFSK modulated signal.

4. Quadrature Partial Response Signalling (QPRS)

Quadrature Partial Response Signalling (QPRS) represents a specific type of the general class of digital signal modulation techniques called Partial Response Signalling. Partial Response Signalling is a method in which a controlled amount of intersymbol interference (ISI) is allowed during the encoding process. Previously any overlap in successive signals resulted in aliasing and an increased probability of error in decoding. The idea was

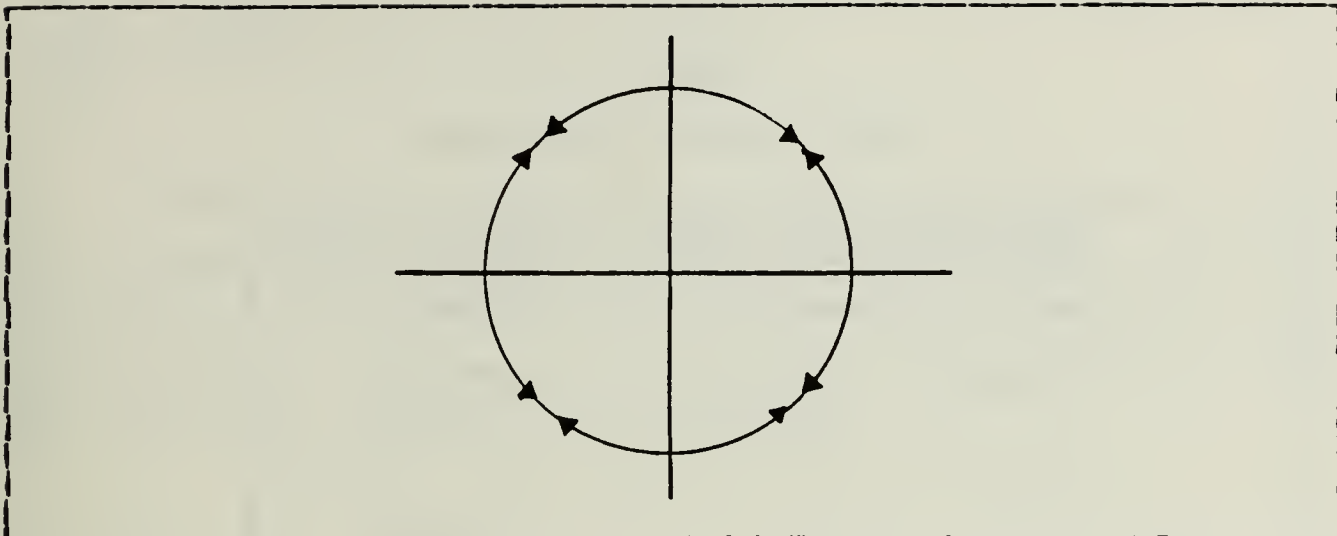


Figure 5.16 Phasor Diagram of FFSK or MSK

first introduced by Lender in 1963 [Ref. 12]. His concept was that in knowing and controlling the amount of interference allowed during the encoding process, compensations can then be made for the ISI at the receiver. Allowing for a limited amount of ISI makes it possible to transmit at rates equal to the Nyquist rate, something that is not possible with many other systems [Ref. 13].

QPRS is implemented, as with previous quadrature systems, through simultaneous modulation of the quadrature components of a common carrier. However, this time the modulation is accomplished with a PRS system. The modulation of the respective quadrature components represents the impulse response of one of a number of linear filters to the bits of the baseband waveform. The linear filter employed depends on the class of the Partial Response Signalling system being used. There are 5 classes of linear filters commonly used in PRS and they are illustrated analytically in Table 1 and graphically in Figure 5.17.

Output of a QPRS system can be represented as in equation 5.16, where a_n and b_n represent the n th bit to be modulated and $h(t - nT_s)$ represents the contribution of the

TABLE 1
QPRS SYSTEM POLYNOMIALS

SYSTEM POLYNOMIAL $F(D)$	FREQUENCY RESPONSE $H(\omega)$ for $ \omega \leq \pi/T$	IMPULSE RESPONSE $h(t)$
$1 + D$	$2T \cos \frac{\omega T}{2}$	$\frac{4T}{\pi} \frac{\cos(\pi t/T)}{T^2 - 4t^2}$
$1 + 2D + D^2$	$4T \cos^2 \frac{\omega T}{2}$	$\frac{2T^3}{\pi} \frac{\sin(\pi t/T)}{T^2 - t^2}$
$2 + D - D^2$	$T + T \cos \omega T + j3T \sin \omega T$	$\frac{T^2}{\pi} \frac{\sin(\pi t/T) (\frac{3t-T}{t^2-T^2})}{t^2 - T^2}$
$1 - D^2$	$j3T \sin \omega T$	$\frac{2T^2}{\pi} \frac{\sin(\pi t/T)}{t^2 - T^2}$
$1 - 2D^2 + D^4$	$-4T \sin^2 \omega T$	$\frac{8T^3}{\pi} \frac{\sin(\pi t/T)}{t^2 - 4T^2}$

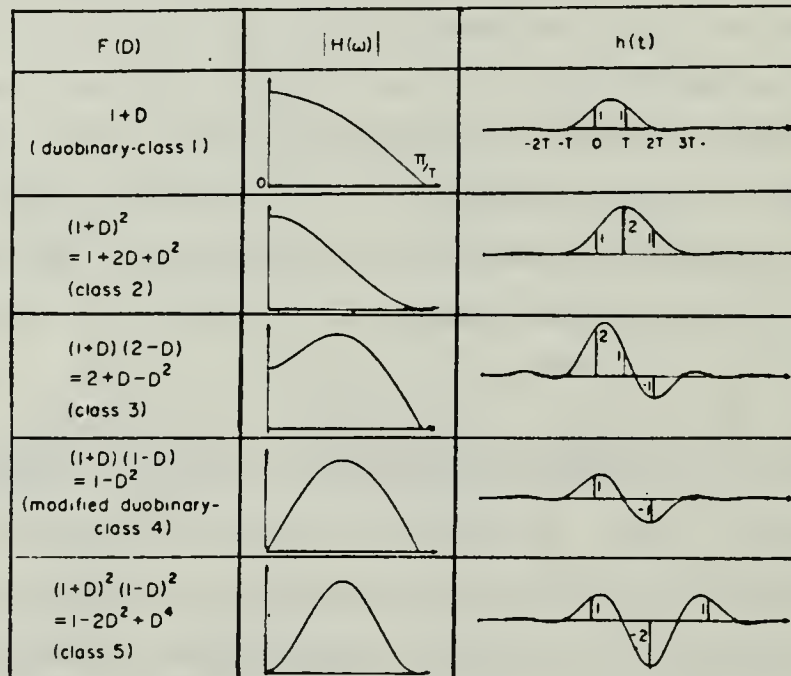


Figure 5.17 QPRS Linear Filter Impulse Responses

impulse response of the linear filter at time t for bit n .
[Ref. 14]

$$v_c(t) = \sum_{n=-\infty}^{\infty} a_n h(t - n T_s) \cos(\omega t + \delta) + \sum_{n=-\infty}^{\infty} b_n h(t - n T_s) \sin(\omega t + \delta) \quad (\text{eqn 5.16})$$

QPRS has the advantage of rapid transmission rates with no increase in bandwidth and excellent error handling performance. The cost of such performance improvement comes in the form of a higher required signal to noise (SNR) ratio when compared to other binary systems.

VI. COMPUTER SIMULATION OF DIGITAL SIGNAL MODULATION TECHNIQUES

Due to the nature of digital signal modulation, it is possible to simulate systems through the use of the digital computer. This chapter is a description of the computer simulation included in the Appendix of this thesis.

A. GENERAL DESCRIPTION OF THE PROGRAM

The program was constructed using top-down design and modular programming. FORTRAN was selected as the programming language due to its capabilities in the area of numerical operations and the availability of mathematical routines to be used as modules in the program. Testing was accomplished on each module as the program was developed. The program was designed to be used interactively in order to allow for instructional use. Although the program was made user friendly in that error checking is accomplished on user inputs, care must be taken to insure instructions are followed correctly.

The program consists of twenty modules, sixteen of which were written by the author, three which were taken from the Double Precision International Mathematics and Statistics Library (IMSLDP) and one which was taken from a NON-IMSL library which resides on the IBM 3033 located at the Naval Postgraduate School. The IBM 3033 was used exclusively for development and testing.

The development was accomplished using the WATFIV compiler; however, the program was written to operate with the VS FORTRAN compiler as well. Testing and operation was done using the VS FORTRAN compiler. Figure 6.1 is a block

diagram of the relationship of the modules for a representative modulation subroutine.

B. MAIN CONTROL MODULE

MAIN operates as the control module for the entire computer simulation and accomplishes limited output. It introduces the program and allows the user to input various parameters of the digital signal modulation technique to be simulated and various other control functions. These inputs include:

1. Modulation technique
2. Class of QPRS system (when appropriate)
3. Digital logic scheme
4. Baud or symbol rate
5. Bits/binary code word (when appropriate)
6. Carrier frequency
7. Number of samples to be generated
8. Carrier max amplitude
9. Initial phase angle
10. Use of random number generator or no
11. Seed for RNG (when appropriate)
12. Number of repetitions of the simulation

Once the user has input the desired characteristics of the modulation to be simulated, MAIN calls the appropriate module to begin the actual calculation. The values necessary to calculate the time series of the signal are passed to the subroutines as parameters. MAIN calls the required subroutine the number of times the user specifies as repetitions. Each call to a subroutine produces the Discrete Fourier Transform and amplitude spectrum of the signal. It is these respective amplitude spectrums which produce the statistics in the final output after MAIN calls the statistics subroutine the final time.

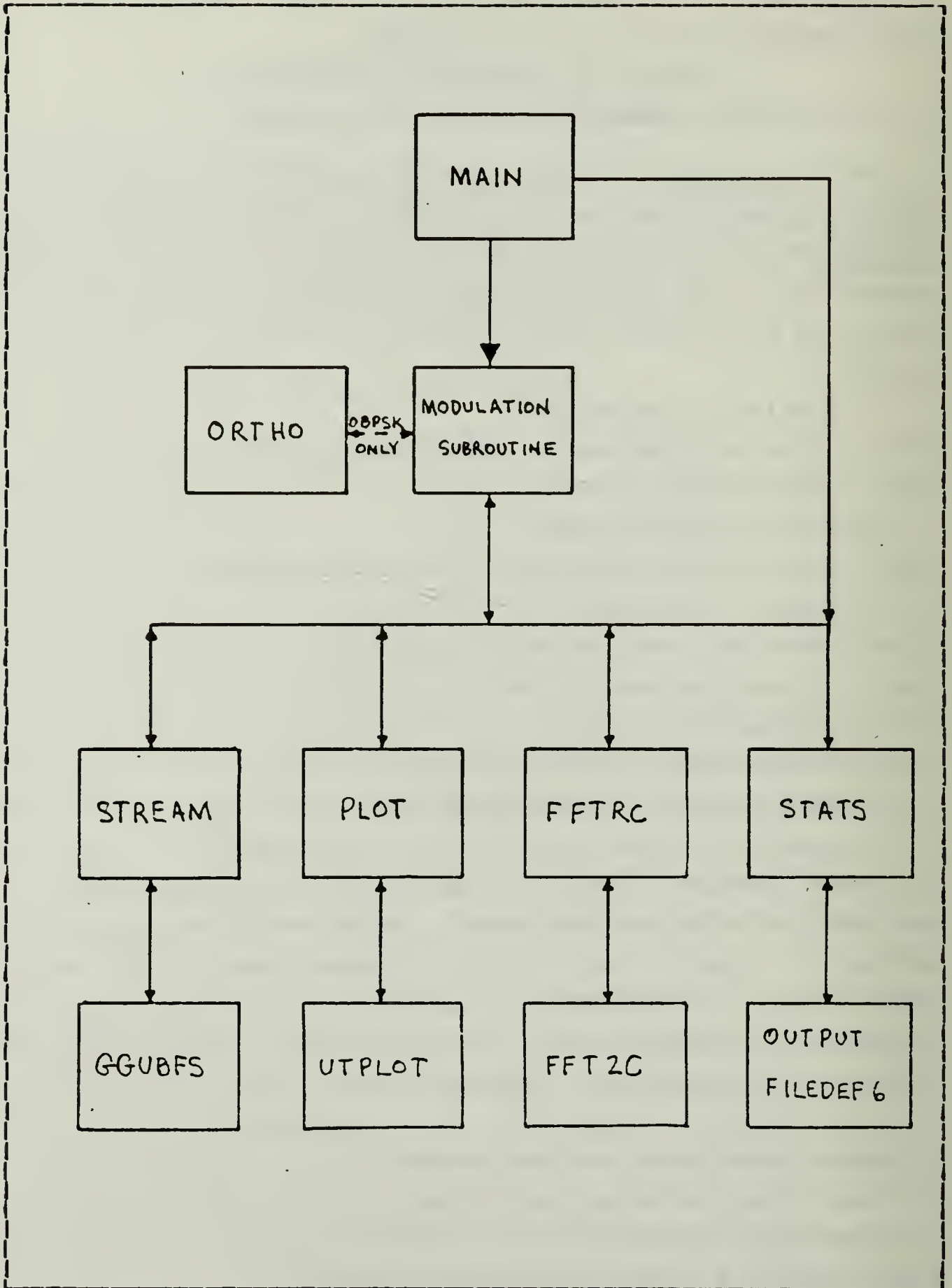


Figure 6.1 Representative Block Diagram

C. SUBROUTINE BPSK

This description of SUBROUTINE BPSK, a module that simulates Binary Phase Shift Keying, will serve as a guide on the construction and operation of subsequent modules involved in the actual signal modulation. A complete description including its interaction with other program subroutines will be included. Since other signal modulation subroutines interact in the same manner within the program, subsequent descriptions will concentrate on differences to this basic module.

SUBROUTINE BPSK begins with variable declarations as with all FORTRAN programs. All variables are declared to be either type integer or double precision. All calculations in the program are carried out in double precision accuracy.

Variable initialization is next. Significant variable initialized at this point are TIME, the time of the first sample which is set to 0. STEP, the delta time between samples is set to the normalized Nyquist sampling rate. OMEGA, the angular frequency and DELTA, the initial phase angle are computed in radians. NBAUD, a variable which keeps track of the number of symbols which have been modulated, is set to 1 or the first symbol is being modulated. NBAUD remains at its present value until total elapsed time exceed 1 symbol duration or BAUDD, the normalized baud rate.

Subsequently, an initial call is made to SUBROUTINE STREAM to receive the value of the first bit to be modulated. The modulation is then carried out according to equation 6.1.

The values of each sample are assigned to an array for storage along with the corresponding time increment. Modulation continues with the first drawn bit until 1 bit or symbol duration is exceeded when STREAM is called to draw

$$v_c(t) = A v(t) \cos(\omega t + \delta)$$

(eqn 6.1)

A = amplitude

v(t) = bit to be modulated

w = angular frequency

t = time

delta = initial phase angle

another bit. This entire process is repeated until the number of samples specified by the user in MAIN is reached.

At this point, only on the first repetition of the simulation, SUBROUTINE PLOT is called which gives the user the opportunity to plot the time series of the simulated signal. Upon return from PLOT the subroutine calls the IMSL routine FFTRC to generate the Discrete Fourier Transform of the time series produced. This is accomplished on each repetition of the program.

Again on the first repetition only, information on the number of the principle harmonic of the FFT is displayed. Plot is called again to give the user the opportunity to plot the amplitude spectrum. The values of the FFT and the amplitude spectrum are computed on each successive repetition of the program and the amplitude spectrum is added to the statistics being accumulated by a call to SUBROUTINE STATS.

D. SUBROUTINE DBPSK

SUBROUTINE DBPSK simulated Differential Binary Phase Shift Keying and is essentially the same as SUBROUTINE BPSK. The difference lies in the fact that what is encoded during the modulation process is the product of the random bit drawn and the value of the bit previously modulated. A

reference bit equal to +1 is used to determine the first bit to be modulated. In this manner, modulation of +1 means no change occurs between successive bits and the phase of the carrier remains the same. Modulation of a -1 indicates a change of bits has occurred and is indicated by a change of phase of the carrier between successive bit durations. The rest of the module remains unchanged.

E. SUBROUTINE OBPSK

Orthogonal Binary Phase Shift Keying is accomplished in this module. Again SUBROUTINE OBPSK is constructed essentially the same as SUBROUTINE BPSK. In Orthogonal BPSK the only bit streams that are modulated are n bits long representing each binary code word, where $n = 2^{*k}$ ($k =$ number of bits per word is limited to 6 bits in MAIN). Each sequence of n bits is orthogonal to every other allowed sequence.

The way this is accomplished in this module is first to draw a series of k random bits from SUBROUTINE STREAM. This series of k 1's and 0's is then changed to its decimal equivalent from 0 to $2^{*k}-1$ and saved for later use.

The program continues with a call to SUBROUTINE ORTHO which generates an $n \times n$ orthogonal matrix of +1's and -1's through the use of the Hadamard matrix and the Kronecker product [Ref. 15]. The Hadamard matrix is a 2×2 orthogonal matrix of 1's and -1's. The Kronecker product is the matrix which is formed when a matrix is expanded to twice its original size by replacing each element of the Hadamard matrix by the product of the Hadamard matrix and the original matrix. The value of the decimal equivalent to the k random bits is used to identify the row of the matrix and the respective columns represent the value of the binary digit which is modulated onto the carrier by BPSK. This

sequence continues until either one bit duration is exceeded, when another orthogonal bit is received from ORTHO or when all the orthogonal bits in a row are modulated. Then another sequence of k random bits is converted to its decimal equivalent and a new row and column of the orthogonal matrix is identified. Execution continues in this manner until all required samples have been produced. It should be noted that the bit rate for Orthogonal BPSK is n times the baud rate. This significantly increases the signal bandwidth requirement and decreases the time increment between successive samples in the simulation. The rest of the module is the same as those previously presented.

F. SUBROUTINE QPSK

Quadrature Phase Shift Keying, simulated in SUBROUTINE QPSK, is accomplished through simultaneous BPSK modulation of the quadrature components of the carrier. Two random bits are drawn from successive calls of SUBROUTINE STREAM and each bit is in turn modulated onto the carrier components and the sum formed. This process is repeated at time intervals equal to the normalized Nyquist sampling rate until TIME exceeds one symbol duration, BAUDD. At this time two new random bits are drawn and the modulation continues until all required samples are produced. The rest of the modules is the same as those before. Equation 6.2 represents the analytical expression used to simulate

G. SUBROUTINE OQPSK

SUBROUTINE OQPSK is essentially the same as SUBROUTINE QPSK with these minor deviations. The time of the first sample is artificially initialized as $TIME = .5(BAUDD)$ or $1/2$ the symbol duration. In this manner, the two random

$$v_c(t) = A v_1(t) \cos(\omega t + \delta) + A v_2(t) \sin(\omega t + \delta) \quad (\text{eqn 6.2})$$

$v_1(t)$ = in-phase bit

$v_2(t)$ = quadrature bit

bits first being modulated are both known to have existed on the carrier for 1/2 the symbol duration. The first of these two bits only remains on the carrier until $\text{TIME} = 1(\text{BAUDD})$ when a third random bit is drawn and modulation begins with this bit. The second random bit is allowed to remain until $\text{TIME} = 1.5(\text{BAUDD})$ when a fourth random bit is drawn to replace it and so on. In this manner the two bits being modulated are offset in the time they change by 1/2 the symbol duration. This necessitates keeping track of the number of bits modulated on both the in-phase and quadrature component of the carrier. The remaining portion of the module is the same as SUBROUTINE QPSK.

H. SUBROUTINE MPSK

This module simulates M-ary Phase Shift Keying. This is accomplished by changing the phase of the carrier to any one of $n = 2^k$ phases where k is the number of bits in the binary code word. The max length of the binary code word is limited to 10 in the MAIN program. This modulation is accomplished by use of equation 6.3 to simulate the MPSK system.

The program first draws k random bits and converts them to the decimal equivalent. At this point modulation begins at $\text{TIME} = 0$ according to equation 6.3. Modulation continues until one symbol duration is exceeded when a new set of k random bits is drawn, conversion to decimal takes place and

$$vc(t) = A \cos[wt + (2\pi m)/n + \delta] \quad (\text{eqn 6.3})$$

m = decimal equivalent of binary code word

$n = 2^{**k}$; k = bits in binary code word

modulation continues or until all desired samples have been produced. The program continues as in previous subroutines.

I. SUBROUTINE MASK

The principles of operation of SUBROUTINE MASK is similar to SUBROUTINE MPSK which also involves a group encoding system. SUBROUTINE MASK allows for M-ary Amplitude Shift Keying. The analytic expression used in the simulation is provided in equation 6.4 A_i is one of 2^{**k} equally spaced amplitudes.

$$vc(t) = A_i \cos(wt + \delta) \quad (\text{eqn 6.4})$$

Once again a set of k random bits is drawn from SUBROUTINE STREAM. The decimal equivalent of the k bits is computed and used to adjust the amplitude A_i according to the assignment routine expressed in equation 6.5.

$$A_i = A/m \quad (\text{eqn 6.5})$$

A = max amplitude

$m = 1$ to n ; $n = 2^{**k}$

This process is repeated at each symbol duration until all desired samples have been produced. The rest of the module remains unchanged.

J. SUBROUTINE QASK

SUBROUTINE QASK combines the elements of the previously described amplitude modulation technique with the now familiar quadrature modulation technique. Two separate streams of random numbers are generated and converted to their decimal form. These numbers are used to produce two separate amplitudes with the same assignment scheme used in MASK. These amplitudes modulate the quadrature components of a common carrier and the output is formed by the sum of the quadratures. Modulation continues in the above manner until a symbol duration elapses when two new amplitudes are calculated. Processing terminates when all required samples are computed.

K. SUBROUTINE MSK

Minimum Shift Keying is frequency shift keying in which the modulation index is $1/2$. The modulation index is represented in equation 6.6

$$h = .5 = (\text{delta}f) T_b \quad (\text{eqn } 6.6)$$

$\text{delta}f$ = frequency separation

T_b = bit duration

The frequency deviation from the carrier is $.5(\text{delta}f) = 1/4T_b$. Converting this frequency deviation to radians yields $\pi/2T_b$. This angular frequency deviation from the central carrier is either $\pm\pi/1T_b$ depending on the value of the bit to be modulated.

The simulation in SUBROUTINE MSK is accomplished by drawing a random bit and generating the signal according to equation 6.7.

$$vc(t) = A \cos[(\omega \pm \pi/2T_b)t + \delta] \quad (\text{eqn 6.7})$$

Once again modulation continues until one bit duration is elapsed when another bit is drawn. Modulation stops when all required samples are produced. The rest of the subroutine remains unchanged.

L. SUBROUTINE MFSK

This subroutine modulates a signal simulating M-ary Frequency Shift Keying. The separation between adjacent frequencies is established as $1/T_s$, where T_s is the symbol duration. This amounts to a modulation index equal to 1. Initially the entire range of frequency deviation from the carrier is calculated as $(n-1)T_s$. The mean frequency deviation is then calculated. In other words the range of frequencies of the modulated signal is the frequency of the central carrier $\pm 1/2$ the magnitude of the entire range of frequency deviation. The minimum frequency is used as the base for computing the frequency to be used to modulate the signal during each respective symbol duration.

At this point in the subroutine a series of k random bits ($k \leq 10$) is drawn and converted to decimal. This decimal number is multiplied by the frequency separation and added to the minimum frequency and converted to radians. The analytical expression of the signal produced with this subroutine is illustrated in equation 6.8.

$$vc(t) = A \cos[(\omega + 2\pi mf)t + \delta] \quad (\text{eqn 6.8})$$

mf = modulation frequency

This modulation continues until a symbol duration elapses when a new frequency deviation or mf is calculated

or modulation stops do to completion of all required samples.

M. SUBROUTINE QPRS

This module simulates 5 different classes of Quadrature Partial Response Signalling systems. The technique employed involves the summation, at each time increment, of all responses to the linear filter representing the class. This is accomplished for all of the bits being modulated during the duration of the simulation.

Initially, two arrays of random bits are generated representing those bits which would be modulated onto the quadrature components of the carrier during the length of time the signal is to be simulated. The the impulse response to each of these n bits is calculated for the time of the respective sample. These impulse responses represent the modulation for the bit in question onto the respective portions of the carrier and the sum is formed according to equation 6.9.

$$v_C(t) = \sum_{n=-\infty}^{\infty} A h(t - nTs) \cos(\omega t + \delta) + \sum_{n=-\infty}^{\infty} A h(t - nTs) \sin(\omega t + \delta) \quad (\text{eqn 6.9})$$

$h(t - nTs) =$ impulse response of nth bit at time t

The time of the first sample is initialized at 6(BAUDD) in order to ensure that when the first sample is taken, contributions from bits modulated at time 0 are also summed do to the overlapping nature of the QPR signals. The value of the last sample is also formed by the sum of the quadrature components existing at 6(BAUDD) after it is produced. The rest of the program operation remains the same as previous modules.

N. SUBROUTINE STREAM

This subroutine interacts with the IMSL random number generator SUBROUTINE GGUBFS to produce a random number between 0 and 1 and make assignment on the basis of the value of this random number to random bits according to the digital logic scheme specified in the MAIN program. It also enables the user to manually insert binary digits if that option was specified previously in MAIN.

O. SUBROUTINE ORTHO

CRTHO produces an $n \times n$ orthogonal matrix from the Hadamard matrix by forming successive Kronecker products [Ref. 15]. It also selects the appropriate row and column of the orthogonal bit to be modulated and passes this bit back to SUBROUTINE OBPSK. Point of entry to SUBROUTINE ORTHO is controlled by a flag set in OBPSK.

P. SUBROUTINE PLOT

PLOT is an interactive module that allows the user to determine whether or not a graph of the output of program calculations is to be produced. The user is also able to selectively vary certain parameters associated with the plot. PLOT calls SUBROUTINE UTPLOT which actually produces the graph and performs the output. UTPLOT is a NON-IMSL library routine from the Naval Postgraduate School.

Q. SUBROUTINE STATS

The statistical calculations associated with the amplitude spectrums of the various functions generated on successive repetitions of the program are computed in SUBROUTINE STATS. Upon completion of each repetition, each module calls STATS where the sum, sum of the squares, sum of

the cubes and sum of the quartics of each element of the amplitude spectrum of the signal produced are computed and stored. When the last repetition of the program is complete, MAIN instructs STATS to compute and output the final statistics, i.e., mean, variance, skewness and kurtosis of each component of the amplitude spectrum according to the estimations contained in [Ref. 16]. Additionally the mean variance and variance of the variance is calculated and output. Point of entrance to this subroutine is controlled by flags set in the individual modulation subroutines or in MAIN.

VII. STATISTICS OF THE FAST FOURIER TRANSFORMS

A. DESCRIPTION OF THE PROBLEM

As stated in Chapter II, if it can be shown that the statistics of the FFT can be somehow linked to a particular digital signal modulation technique, then the modulation technique can be identified on the basis of those statistics alone. Although it is beyond the scope of this thesis to actually derive those relationships if they exist, it seems prudent to attempt to determine if there is statistical differences between the components of the FFT's as they are derived in the enclosed computer simulations.

The statistic chosen to do the hypothesis testing is the F-test since the true mean and variance of the distribution need not be known [Ref. 17]. In addition, the information necessary to calculate the F-statistic is readily accumulated in SUBROUTINE STATS. Calculation of the F-statistic necessitated the writing of a small computer program to be used for that purpose once the output from the main program was generated and reformatted.

B. ANALYSIS-OF-VARIANCE

If there were no differences attributable to the modulation technique, then it would be reasonable to assume that for a certain set of characteristics, the components of successive FFT's would be the same. In other words, if a signal was modulated by BPSK and a statistically significant number of FFT's were generated of the signal, then the statistics of those FFT's would be assumed to be related. On the other hand, if it can be shown that the statistics are not related (i.e., not from the same distribution), then

significance can be placed in the variation among modulation techniques.

1. The F-Distribution

The assumptions necessary to use the F-distribution are:

1. Normal distribution
2. Random samples
3. Independent samples

These assumptions are not too difficult to intuitively accept in the model that will be proposed. Once again it would be expected that the FFT's of successive identically modulated signals to be related. For the simulations conducted as part of this test, they were all generated using bits from a random number generator for which it can be shown that each sequence of bits passes statistical tests for randomness and independence. The assumption of normality could also be argued on the basis of the central limit theorem.

The value of the F-statistic with which comparison will be made is 1.51 for 14 degrees of freedom in the numerator, an infinite number of degrees of freedom in the denominator and a 90% confidence region. How these values were obtained will be detailed under the design of the experiment.

2. Design of the Experiment

The experimental data used in the computation of the statistics was chosen to minimize the random contributions of variables other than the modulation technique. The computer simulations included in this thesis were used to generate the statistics and a separate program also included in the appendix was used to calculate the F-statistic. The variables in the experiment include:

1. Modulation technique
2. Logic type
3. Baud rate
4. Bits per binary code word
5. Carrier frequency
6. Carrier amplitude
7. Initial phase angle
8. Number of samples generated
9. Time between samples
10. Seed for random number generator
11. Number of repetitions or trials

Fifteen different modulation techniques were compared. In all cases bipolar logic was simulated, the baud rate was held constant at 1200 baud and the maximum carrier amplitude was established at 1 volt. Additionally the phase angle of all simulations was 0 degrees and the seed for the random number generator was 1 thereby ensuring the same random sequence of bits. The number of bits per binary code word did vary among the modulation techniques. When the modulation technique was M-ary, the bits per code word was always 3 so it is possible to infer that bits per code word is a function of the modulation technique. The time between samples was the normalized Nyquist sampling rate. This did vary between modulation techniques but was necessary to derive an accurate FFT. Carrier frequency also varied between simulations but was always twice the lowest carrier frequency recommended in the computer simulation. In most cases this was 2400 Hz, or twice the baud rate. Finally each simulation was repeated 100 times and the statistics of the FFT's based on those 100 repetitions. The number of samples produced was always 64 so there are 33 components of the FFT.

What this amounts to can be illustrated through an Analysis-of-Variance table as shown in Table 2 [Ref. 17].

TABLE 2
ANALYSIS-OF-VARIANCE TABLE

n Observations in Each of *r* Groups

		Observations					Sum	Mean
Group	1	Y_{11}	Y_{12}	Y_{13}	Y_{1n}	$Y_{1.}$	$\bar{Y}_{1.}$
	2	Y_{21}	Y_{22}	Y_{23}	Y_{2n}	$Y_{2.}$	$\bar{Y}_{2.}$
	3	Y_{31}	Y_{32}	Y_{33}	Y_{3n}	$Y_{3.}$	$\bar{Y}_{3.}$
	<i>r</i>	Y_{r1}	Y_{r2}	Y_{r3}	Y_{rn}	$Y_{r.}$	$\bar{Y}_{r.}$

In the case of the simulation described above, this amounts to 100 observations (repetitions or trials) from each of 15 groups (modulation techniques) for each of the 33 components of the FFT. The degrees of freedom in the numerator is equal to (15-1) or 14 while the degrees of freedom in the denominator is equal to 15(100-1) or 1485. Table values for the F-distribution use infinity as the degree of freedom for values greater than 120.

An F-test was also performed to determine if there is a relationship among the mean variance, mean skewness or mean kurtosis of the 15 different modulation techniques. Again the assumption is made that these statistics would be normally distributed from modulation techniques which had the same or statistically similar components of their FFT's. In this case there were again 15 modulation techniques to compare (14 degrees of freedom) but only 33 observations (the variance, skewness or kurtosis of the respective elements of the FFT). This number of observations yields 15(33-1) = 480 degrees of freedom in the denominator.

3. Hypothesis and Hypothesis Testing

The hypothesis posed for the model is that the means of the individual components of the FFT's from the 15 modulation techniques are from the same distribution. Therefore, the respective means must be equal. Also tested is that the mean variance, mean skewness and mean kurtosis of all components of the FFT's of each modulation technique are equal. These hypothesis are illustrated in equations 7.1 through equation 7.4. Each hypothesis is tested and compared to the F-distribution selecting a rejection region or level of significance of .9. This equates to an F-statistic of 1.51 for 14 degrees of freedom in the numerator and an infinite number of degrees of freedom in the denominator.

4. Results

The means of the 33 components of the FFT for each of the 15 modulation techniques were compared using the F-distribution. The results are shown in Table 3. Table 4 shows the F-statistics associated with the comparison of the mean of the variance, mean of the skewness and mean of the kurtosis for the respective groups. In addition a complete summation of the results of the F-test are included in the appendix.

C. **CONCLUSION**

The results of the F-test indicate that the null hypothesis must be rejected at the .9 significance level and the alternate hypothesis accepted that the means are not equal for FFT components 9-14. In addition the F-statistic for the comparison of mean variance, mean skewness and mean kurtosis all fall in the rejection area.

$$H_0: \text{XBAR11} = \text{XBAR21} = \dots = \text{XBARij} \quad (\text{eqn 7.1})$$

$$H_1: \text{XBAR11} \neq \text{XBAR21} \neq \dots \neq \text{XBARij}$$

i = i th modulation technique

j = j th component of the FFT

$$H_0: \text{MVAR1} = \text{MVAR2} = \dots = \text{MVAR15} \quad (\text{eqn 7.2})$$

$$H_1: \text{MVAR1} \neq \text{MVAR2} \neq \dots \neq \text{MVAR 15}$$

$$H_0: \text{MSKEW1} = \text{MSKEW2} = \dots = \text{MSKEW15} \quad (\text{eqn 7.3})$$

$$H_1: \text{MSKEW1} \neq \text{MSKEW2} \neq \dots \neq \text{MSKEW15}$$

$$H_0: \text{MKUR1} = \text{MKUR2} = \dots = \text{MKUR15} \quad (\text{eqn 7.4})$$

$$H_1: \text{MKUR1} \neq \text{MKUR2} \neq \dots \neq \text{MKUR15}$$

This indicates that there is a difference between the statistics of the FFT's of the respective modulation technique. Since all the parameters used in the generation of these statistics were held essentially constant among the trials, it can be assumed that these differences are due to the modulation technique employed. It has not been established yet what those differences may be. This is an area where future research and study is warranted.

The results of this test would seem to point to those components of the FFT which offer the best opportunity to develop those relationships or differences. FFT components 9-14 have obvious differences; however, FFT components 20, 24 and 25 also have large F-statistics but do not fall in the rejection area. These components may also be

TABLE 3
F-STATISTICS OF FFT COMPONENTS

FFT COMPONENT	AMONG GROUP SUM	WITHIN GROUP SUM	TOTAL OF SQUARES	F-STAT
1	0.121	17.69	17.81	0.727
2	0.112	18.48	18.59	0.642
3	0.108	20.65	20.76	0.557
4	0.135	25.40	25.54	0.562
5	0.172	32.74	32.91	0.558
6	0.254	41.72	41.98	0.647
7	0.422	50.10	50.52	0.893
8	0.962	82.83	83.79	1.231
9	7.591	390.2	397.8	2.063
10	49.09	1681.0	1730.1	3.097
11	53.01	1732.1	1785.1	3.246
12	61.56	2071.7	2133.3	3.152
13	45.73	1832.8	1878.6	2.646
14	3.864	250.5	254.4	1.636
15	0.539	98.13	98.67	0.582
16	0.366	110.1	110.5	0.353
17	0.504	151.0	151.5	0.354
18	0.943	140.3	141.2	0.713
19	1.299	158.5	159.8	0.870
20	2.671	200.7	203.4	1.412
21	1.853	226.3	228.2	0.868
22	2.277	232.1	234.3	1.041
23	1.712	197.6	199.3	0.919
24	2.512	181.9	184.4	1.476
25	2.144	171.3	173.5	1.327
26	1.257	143.7	145.0	0.928
27	1.233	113.9	115.1	1.149

TABLE 3
F-STATISTICS OF FFT COMPONENTS (con't)

28	0.858	115.8	116.7	0.785
29	0.547	63.72	64.27	0.911
30	0.356	55.77	56.13	0.677
31	0.183	41.41	51.59	0.469
32	0.051	13.79	13.84	0.389
33	0.031	10.92	10.96	0.304

TABLE 4
F-STATISTICS OF THE MEAN VARIANCES,
MEAN SKEWNESS AND MEAN KURTOSIS

	AMONG GROUP SUM	WITHIN GROUP SUM	TOTAL OF SQUARES	F-STAT
VARIANCE	3.144 E5	3.755 E6	4.070 E6	2.870
SKEWNESS	5.307 E10	7.031 E11	7.562 E11	2.588
KURTOSIS	8.280 E11	1.262 E13	1.344 E13	2.250

interesting to examine. In addition, it should be noted that the statistics of the FFT associated with each respective modulation technique also display some striking differences. These statistics may prove in some way to be a fingerprint of the modulation techniques themselves.

MAI 01950
 MAI 01960
 MAI 01970
 MAI 01980
 MAI 01990
 MAI 02000
 MAI 02010
 MAI 02020
 MAI 02030
 MAI 02040
 MAI 02050
 MAI 02060
 MAI 02070
 MAI 02080
 MAI 02090
 MAI 02100
 MAI 02110
 MAI 02120
 MAI 02130
 MAI 02140
 MAI 02150
 MAI 02160
 MAI 02170
 MAI 02180
 MAI 02190
 MAI 02200
 MAI 02210
 MAI 02220
 MAI 02230
 MAI 02240
 MAI 02250
 MAI 02260
 MAI 02270
 MAI 02280
 MAI 02290
 MAI 02300
 MAI 02310
 MAI 02320
 MAI 02330
 MAI 02340
 MAI 02350
 MAI 02360
 MAI 02370
 MAI 02380
 MAI 02390
 MAI 02400
 MAI 02410
 MAI 02420
 MAI 02430
 MAI 02440

```

C      READ (5, *) IBAUD
C      BAUD= IBAUD
C      BAUD=1. DO/ BAUD
C      ** DETERMINE THE BITS EITHER BY THE TYPE OF DIGITAL
C      MODULATION SPECIFIED OR BY USER INPUT ***
C      CALL FRTCMS ('CLRSCRN ')
C      IF (TYPE1.EQ. 1.OR.TYPE1.EQ. 2.OR.TYPE1.EQ. 9) THEN
C          IBITS=1
C          BITS=IBITS
C      ELSE IF (TYPE1.EQ. 3) THEN
79      WRITE(10, 80)
80      FORMAT( ' ENTER THE NUMBER OF BITS IN EACH SYMBOL. ' // OR LESS'
C          ' CAUTION! THE NUMBER OF BITS PER SYMBOL MUST BE 6 OR LESS'
C          ' // ' : ')
C      READ (5, *) IBITS
C      IF (IBITS.LT. 1.OR. IBITS.GT. 6) THEN
C          CALL FRTCMS ('CLRSCRN ')
C          WRITE(10, 90)
C          FORMAT( ' ERROR' //)
C          GO TO 79
C      ELSE
C          BITS=IBITS
C          END IF
C      ELSE IF (TYPE1.EQ. 4.OR.TYPE1.EQ. 5.OR.TYPE1.EQ. 11) THEN
C          IBITS=2
C          BITS=IBITS
C      ELSE IF (TYPE1.GE. 6.OR.TYPE1.LE. 8.OR.TYPE1.EQ. 10) THEN
99      WRITE(10, 100)
100     FORMAT( ' ENTER THE NUMBER OF BITS IN EACH SYMBOL. ' // OR LESS'
C          ' CAUTION! THE NUMBER OF BITS PER SYMBOL MUST BE 10 OR LESS'
C          ' // ' : ')
C      READ (5, *) IBITS
C      IF (IBITS.LT. 1.OR. IBITS.GT. 11) THEN
C          CALL FRTCMS ('CLRSCRN ')
C          WRITE(10, 110)
C          FORMAT( ' ERROR' //)
C          GO TO 99
110

```

```

ELSE      BITS=IBITS
END IF
END IF
*** DETERMINE AND DISPLAY THE BIT RATE ***
IF (TYPE1.EQ.3) THEN
  BITR=(2.D0**IBITS)*BAUD
ELSE
  BITR=BITS*BAUD
END IF
CALL FRTCMS('CLRSCRN ')
WRITE(10,120)BITR
FORMAT(' THE BIT RATE FOR THE SPECIFIED SIGNAL IS',F9.0,' BITS/SEC
*)
*** HAVE THE USER ENTER THE CARRIER FREQUENCY ***
IF (TYPE1.EQ.3) THEN
  FC=BITR
ELSE IF (TYPE1.EQ.9) THEN
  FC={.25D0*BAUD
ELSE IF (TYPE1.EQ.10) THEN
  FC=BAUD+((2.D0**IBITS)-1.D0)*(BAUD/2.D0)
ELSE
  FC=BAUD
END IF
WRITE(10,130)FC
FORMAT(' ENTER THE CARRIER FREQUENCY AT THIS TIME.',F9.0,' // HZ.,//.
* : ')
READ(5,*)IFREQ
FRFQ=IFREQ
IF (FREQ.LT.FC) THEN
  CALL FRTCMS('CLRSCRN ')
  WRITE(10,140)
  FORMAT(' THE CARRIER FREQUENCY IS LESS THAN RECOMMENDED.',/)
  GO TO 149
END IF
*** HAVE THE USER ENTER THE NUMBER OF SAMPLES TO BE GENERATED ***
CALL FRTCMS('CLRSCRN ')

```

```

MAI 02450
MAI 02460
MAI 02470
MAI 02480
MAI 02490
MAI 02500
MAI 02510
MAI 02520
MAI 02530
MAI 02540
MAI 02550
MAI 02560
MAI 02570
MAI 02580
MAI 02590
MAI 02600
MAI 02610
MAI 02620
MAI 02630
MAI 02640
MAI 02650
MAI 02660
MAI 02670
MAI 02680
MAI 02690
MAI 02700
MAI 02710
MAI 02720
MAI 02730
MAI 02740
MAI 02750
MAI 02760
MAI 02770
MAI 02780
MAI 02790
MAI 02800
MAI 02810
MAI 02820
MAI 02830
MAI 02840
MAI 02850
MAI 02860
MAI 02870
MAI 02880
MAI 02890
MAI 02900
MAI 02910
MAI 02920
MAI 02930
MAI 02940

```

```

C 149 WRITE(10,150)
C 150 FORMAT(' ENTER THE NUMBER OF SAMPLES OF THE MODULATED SIGNAL,
* TO BE PRODUCED. THIS NUMBER MUST BE EQUAL TO 2**N
* WHERE N IS A POSITIVE INTEGER EQUAL TO OR LESS THAN 10.://,
* I.E., 2, 4, 8, ..., 1024.://,')
C READ(5,*) IN
C N=IN
C IF(IN.EQ.2.OR.IN.EQ.4.OR.IN.EQ.8.OR.IN.EQ.16.OR.IN.EQ.32.OR.
*IN.EQ.64.OR.IN.EQ.128.OR.IN.EQ.256.OR.IN.EQ.512.OR.IN.EQ.1024) THEN
GO TO 170
ELSE
CALL FRTCMS(' CLRSCRN ')
WRITE(10,160)
FORMAT(' ERROR ',/)
GO TO 149
END IF
C *** DETERMINE AND DISPLAY INFO ABOUT THE RECORD LENGTH ***
C 160 IF (TYPE1.EQ.2) THEN 0*((FREQ+BITR))
ELSE STEP=1.D0/(2.D0*(FREQ+BITR))
ELSE STEP=1.D0/(2.D0*(FREQ+(1.25D0*BAUD)))
ELSE IF (TYPE1.EQ.10) THEN
STEP=1.D0/(2.D0*((FREQ+((2.D0**IBITS)-1.)*(BAUD/2.D0))+BAUD))
ELSE IF (TYPE1.EQ.11) THEN
STEP=1.D0/(2.D0*((PI+1.D0)*BAUD))
ELSE
STEP=1.D0/(2.D0*(FREQ+BAUD))
END IF
C IF (TYPE1.EQ.3.AND.((N-1.)*STEP).LE.1./BITR) THEN
C CALL FRTCMS(' CLRSCRN ')
C 180 WRITE(10,180)
FORMAT(' ELAPSED TIME FOR SIGNAL GENERATION WILL BE LESS THAN
// INCREASING THE NUMBER OF SAMPLES TO BE PRODUCED, BAUD
// INCREASING CARRIER FREQUENCY, BY DECREASING THE
// RATE OR BY DECREASING THE SIZE OF THE BINARY CODE WORD.
// ENTER ANY OTHER INTEGER VALUE TO CONTINUE.://,')
C READ(5,*) ANS
C IF (ANS.EQ.1) THEN
GO TO 29
END IF

```

```

MAI 02950
MAI 02960
MAI 02970
MAI 02980
MAI 02990
MAI 03000
MAI 03010
MAI 03020
MAI 03030
MAI 03040
MAI 03050
MAI 03060
MAI 03070
MAI 03080
MAI 03090
MAI 03100
MAI 03110
MAI 03120
MAI 03130
MAI 03140
MAI 03150
MAI 03160
MAI 03170
MAI 03180
MAI 03190
MAI 03200
MAI 03210
MAI 03220
MAI 03230
MAI 03240
MAI 03250
MAI 03260
MAI 03270
MAI 03280
MAI 03290
MAI 03300
MAI 03310
MAI 03320
MAI 03330
MAI 03340
MAI 03350
MAI 03360
MAI 03370
MAI 03380
MAI 03390
MAI 03400
MAI 03410
MAI 03420
MAI 03430
MAI 03440

```

```

C      ELSE IF ((N-1.D0)*STEP).LE.BAUDD) THEN
C      CALL FRTCMS('CLRSCRN ')
C      WRITE(10,190)
190    FORMAT(1,'ELAPSED TIME FOR SIGNAL GENERATION WILL BE LESS THAN',
*      /,'SYMBOL DURATION. IF YOU WISH TO CHANGE THIS BY',
*      /,'INCREASING CARRIER FREQUENCY, BY DECREASING THE BAUDD',
*      /,'DECREASING CARRIER FREQUENCY, BY DECREASING THE BAUDD',
*      /,'RATE OR BY INCREASING THE SIZE OF THE BINARY CODE WORD',
*      /,'ENTER A 1. ENTER ANY OTHER INTEGER VALUE TO CONTINUE',
*      /,'WITH THE SIMULATION AS SPECIFIED.',//,':')
C      READ(5,*)ANS
C      IF(ANS.EQ.1) THEN
C      GO TO 29
C      END IF
C      END IF
C      *** HAVE THE USER ENTER THE AMPLITUDE OF THE CARRIER WAVE ***
C      CALL FRTCMS('CLRSCRN ')
199    WRITE(10,200)
200    FORMAT(1,'ENTER THE AMPLITUDE OF THE CARRIER.',//,':')
C      READ(5,*)IAMP
C      AMP=IAMP
C      *** HAVE THE USER ENTER THE INITIAL PHASE ANGLE ***
C      CALL FRTCMS('CLRSCRN ')
209    WRITE(10,210)
210    FORMAT(1,'ENTER THE INITIAL PHASE ANGLE FROM 0 TO 360 DEGREES.',//,':')
C      READ(5,*)IIPHAS
C      IF(IIPHAS.LT.0.OR.IIPHAS.GT.360) THEN
C      CALL FRTCMS('CLRSCRN ')
C      WRITE(10,220)
220    FORMAT(1,'ERROR',/)
C      GO TO 209
C      ELSE
C      IPHAS=IIPHAS
C      END IF
C

```

```

MAI 03450
MAI 03460
MAI 03470
MAI 03480
MAI 03490
MAI 03500
MAI 03510
MAI 03520
MAI 03530
MAI 03540
MAI 03550
MAI 03560
MAI 03570
MAI 03580
MAI 03590
MAI 03600
MAI 03610
MAI 03620
MAI 03630
MAI 03640
MAI 03650
MAI 03660
MAI 03670
MAI 03680
MAI 03690
MAI 03700
MAI 03710
MAI 03720
MAI 03730
MAI 03740
MAI 03750
MAI 03760
MAI 03770
MAI 03780
MAI 03790
MAI 03800
MAI 03810
MAI 03820
MAI 03830
MAI 03840
MAI 03850
MAI 03860
MAI 03870
MAI 03880
MAI 03890
MAI 03900
MAI 03910
MAI 03920
MAI 03930
MAI 03940

```



```

C      ELSE IF (TYPE1.EQ.2) THEN
C      CALL DBPSK(TYPE2, BAUD, FREQ, IPHAS, AMP, ANS2, DSEED, IN, REP)
C
C      ELSE IF (TYPE1.EQ.3) THEN
C      CALL OBPSK(TYPE2, BAUD, BITS, FREQ, IPHAS, AMP, ANS2, DSEED, IN, REP)
C
C      ELSE IF (TYPE1.EQ.4) THEN
C      CALL QPSK(TYPE2, BAUD, BITS, FREQ, IPHAS, AMP, ANS2, DSEED, IN, REP)
C
C      ELSE IF (TYPE1.EQ.5) THEN
C      CALL OQPSK(TYPE2, BAUD, BITS, FREQ, IPHAS, AMP, ANS2, DSEED, IN,
*      REP)
C
C      ELSE IF (TYPE1.EQ.6) THEN
C      CALL MPSK(TYPE2, BAUD, BITS, FREQ, IPHAS, AMP, ANS2, DSEED, IN,
*      REP)
C
C      ELSE IF (TYPE1.EQ.7) THEN
C      CALL MASK(TYPE2, BAUD, BITS, FREQ, IPHAS, AMP, ANS2, DSEED, IN,
*      REP)
C
C      ELSE IF (TYPE1.EQ.8) THEN
C      CALL QASK(TYPE2, BAUD, BITS, FREQ, IPHAS, AMP, ANS2, DSEED, IN,
*      REP)
C
C      ELSE IF (TYPE1.EQ.9) THEN
C      CALL MSK(TYPE2, BAUD, FREQ, IPHAS, AMP, ANS2, DSEED, IN, REP)
C
C      ELSE IF (TYPE1.EQ.10) THEN
C      CALL MFSK(TYPE2, BAUD, BITS, FREQ, IPHAS, AMP, ANS2, DSEED, IN, REP)
C
C      ELSE IF (TYPE1.EQ.11) THEN
C      CALL OPFS(TYPE2, TYPE3, BAUD, BITS, FREQ, IPHAS, AMP, ANS2, DSEED,
*      IN, REP)
C
C      END IF
C
C      CONTINUE
C 280
C      ** OUTPUT A FINGERPRINT OF THE MODULATION ACCOMPLISHED ***
C
C      IF (TYPE1.EQ.1) THEN
C      WRITE(6, 1, MODULATION TECHNIQUE = BPSK')
C 281
C      ELSE IF (TYPE1.EQ.2) THEN
C      WRITE(6, 2, MODULATION TECHNIQUE = DBPSK')
C 282
C      ELSE IF (TYPE1.EQ.3) THEN
C      WRITE(6, 283)

```

```

MAI 04450
MAI 04460
MAI 04470
MAI 04480
MAI 04490
MAI 04500
MAI 04510
MAI 04520
MAI 04530
MAI 04540
MAI 04550
MAI 04560
MAI 04570
MAI 04580
MAI 04590
MAI 04600
MAI 04610
MAI 04620
MAI 04630
MAI 04640
MAI 04650
MAI 04660
MAI 04670
MAI 04680
MAI 04690
MAI 04700
MAI 04710
MAI 04720
MAI 04730
MAI 04740
MAI 04750
MAI 04760
MAI 04770
MAI 04780
MAI 04790
MAI 04800
MAI 04810
MAI 04820
MAI 04830
MAI 04840
MAI 04850
MAI 04860
MAI 04870
MAI 04880
MAI 04890
MAI 04900
MAI 04910
MAI 04920
MAI 04930
MAI 04940

```

MAI 04950
 MAI 04960
 MAI 04970
 MAI 04980
 MAI 04990
 MAI 05000
 MAI 05010
 MAI 05020
 MAI 05030
 MAI 05040
 MAI 05050
 MAI 05060
 MAI 05070
 MAI 05080
 MAI 05090
 MAI 05100
 MAI 05110
 MAI 05120
 MAI 05130
 MAI 05140
 MAI 05150
 MAI 05160
 MAI 05170
 MAI 05180
 MAI 05190
 MAI 05200
 MAI 05210
 MAI 05220
 MAI 05230
 MAI 05240
 MAI 05250
 MAI 05260
 MAI 05270
 MAI 05280
 MAI 05290
 MAI 05300
 MAI 05310
 MAI 05320
 MAI 05330
 MAI 05340
 MAI 05350
 MAI 05360
 MAI 05370
 MAI 05380
 MAI 05390
 MAI 05400
 MAI 05410
 MAI 05420
 MAI 05430
 MAI 05440

```

283     ELSE FORMAT('1', MODULATION TECHNIQUE = ORTHOGONAL BPSK')
        IF (TYPE(6, EQ. 4) THEN
284     FORMAT('1', MODULATION TECHNIQUE = QPSK')
        IF (TYPE(6, EQ. 5) THEN
285     FORMAT('1', MODULATION TECHNIQUE = OQPSK')
        IF (TYPE(6, EQ. 6) THEN
286     FORMAT('1', MODULATION TECHNIQUE = MPSK')
        IF (TYPE(6, EQ. 7) THEN
287     FORMAT('1', MODULATION TECHNIQUE = MASK')
        IF (TYPE(6, EQ. 8) THEN
288     FORMAT('1', MODULATION TECHNIQUE = QASK')
        IF (TYPE(6, EQ. 9) THEN
289     FORMAT('1', MODULATION TECHNIQUE = MSK')
        IF (TYPE(6, EQ. 10) THEN
290     FORMAT('1', MODULATION TECHNIQUE = MFSK')
        IF (TYPE(6, EQ. 11) THEN
291     FORMAT('1', MODULATION TECHNIQUE = QPRS')
    C
292     IF (TYPE(6, EQ. 11) AND .TYPE3.EQ.1) THEN
        WRITE(6, QPRS CLASS 1 FILTER')
        IF (TYPE(6, EQ. 11) AND .TYPE3.EQ.2) THEN
293     WRITE(6, QPRS CLASS 2 FILTER')
        IF (TYPE(6, EQ. 11) AND .TYPE3.EQ.3) THEN
294     WRITE(6, QPRS CLASS 3 FILTER')
        IF (TYPE(6, EQ. 11) AND .TYPE3.EQ.4) THEN
295     WRITE(6, QPRS CLASS 4 FILTER')
        IF (TYPE(6, EQ. 11) AND .TYPE3.EQ.5) THEN
296     WRITE(6, QPRS CLASS 5 FILTER')
    C
297     IF (TYPE(6, EQ. 1) THEN
        WRITE(6, BIPOLAR LOGIC')
        IF (TYPE(6, EQ. 2) THEN
298     WRITE(6, UNIPOLAR POSITIVE LOGIC')

```


MAI 05950
MAI 05960
MAI 05970
MAI 05980
MAI 05990
MAI 06000
MAI 06010
MAI 06020
MAI 06030
MAI 06040
MAI 06050
MAI 06060
MAI 06070
MAI 06080
MAI 06090
MAI 06100
MAI 06110

```
END IF  
*** DETERMINE IF ANOTHER SIMULATION IS TO BE RUN ***  
WRITE(10,330)  
FORMAT(' ENTER A 1 IF YOU DESIRE TO SIMULATE ANOTHER SIGNAL: ',//, ': ',//)  
* ENTER ANY OTHER INTEGER IF YOU ARE READY TO QUIT. '//, ': ',//)  
READ (5,*)ANS  
IF (ANS.EQ.1) THEN  
  CALL FRTCMS('CLRSCRN ')  
  GO TO 29  
END IF  
STOP  
END
```

C
C
C
330
C
C
C
C

BPS00110
BPS00120
BPS00130
BPS00140
BPS00150
BPS00160
BPS00170
BPS00180
BPS00190
BPS00200
BPS00210
BPS00220
BPS00230
BPS00240
BPS00250
BPS00260
BPS00270
BPS00280
BPS00290
BPS00300
BPS00310
BPS00320
BPS00330
BPS00340
BPS00350
BPS00360
BPS00370
BPS00380
BPS00390
BPS00400
BPS00410
BPS00420
BPS00430
BPS00440
BPS00450
BPS00460
BPS00470
BPS00480
BPS00490
BPS00500
BPS00510
BPS00520
BPS00530
BPS00540
BPS00550
BPS00560
BPS00570
BPS00580
BPS00590
BPS00600

```
SUBROUTINE BPSK (TYPE2, BAUD, FREQ, IPHAS, AMP, ANS2,  
*DSEED, IN, REP)  
*** PURPOSE ***  
THIS SUBROUTINE MODULATES THE CARRIER USING BINARY PHASE SHIFT  
KEYING AS THE MODULATION TECHNIQUE.  
*** PARAMETER DEFINITIONS ***  
TYPE2= INDICATES LOGIC TYPE TO BE EMPLOYED  
BAUD= SYMBOL RATE OR BAUD RATE  
FREQ= CARRIER FREQUENCY  
IPHAS= INITIAL PHASE ANGLE IN DEGREES  
AMP= AMPLITUDE  
ANS2= INTEGER VARIABLE TO BE PASSED TO STREAM GENERATOR  
DSEED= DOUBLE PRECISION SEED FOR RANDOM NUMBER GENERATOR  
IN= NUMBER OF POSITIONS IN ARRAY TO BE UTILIZED  
REP= AN INTEGER EQUAL TO THE NUMBER OF THE REPETITION OF  
THE CALL THE THIS SUBROUTINE  
*** VARIABLE DEFINITIONS ***  
ARRAY= A DOUBLE PRECISION ARRAY FOR PASSING THE BINARY  
DIGITS AND STORING THE VALUE OF THE TIME FUNCTION  
AND THE FFT  
R= AN INTEGER USED TO REPRESENT THE ROW OF ARRAY  
TIME= TIME VARIABLE  
MT= VALUE OF THE BINARY DIGIT  
STEP= INTERVAL AT WHICH THE SIGNAL IS REPRODUCED  
PI= NUMERICAL CONSTANT  
OMEGA= CARRIER ANGULAR FREQUENCY  
DELTA= INITIAL PHASE OFFSET IN RADIANS  
NBAUD= A COUNT OF THE NUMBER OF BAUDS MODULATED  
BAUDD= BAUD DURATION  
X= COMPLEX ARRAY TO RECEIVE THE FFT OF THE TIME SERIES  
IWK= INTEGER WORKING ARRAY USED BY FUNCTION FFTC  
MAXY= MAXIMUM VALUE TO BE PLOTTED ON THE ABCISSAE  
MINY= MINIMUM VALUE TO BE PLOTTED ON THE ABCISSAE  
INT= INTERVAL BETWEEN POINTS ON THE ORDINATE  
RMAX= VALUE OF THE PRINCIPLE HARMONIC  
FLAG= AN INTEGER WHICH CONTROL ENTRANCE AND EXIT FROM  
SUBPROGRAM STATS  
IND2P1= ARRAY LENGTH DIVIDED BY 2 PLUS 1  
*** VARIABLE DECLARATIONS ***  
INTEGER R, ANS2, TYPE2, IN, RMAX, REP, FLAG, IND2P1  
DOUBLE PRECISION BAUD, FREQ, IPHAS, AMP, TIME, MT,
```

CC

```

C          C STEP, PI, OMEGA, DELTA, NBAUD, BAUDD,
C          C *DSEED, MAXY, MINY, INT
C          C DOUBLE PRECISION ARRAY(1024, 2), SUMX(513), SUMXSQ(513), SUMX3(513),
C          C *SUMX4(513)
C          C COMMON ARRAY, SUMX, SUMXSQ, SUMX3, SUMX4
C          C COMPLEX*16 X(513)
C          C INTEGER IWK(10)
C          C *** VARIABLE INITIALIZATION ***
C          C R=1
C          C TIME=0. DO
C          C STEP=1. DO/(2. DO*(FREQ+BAUD))
C          C PI=3.141592653589793D0
C          C OMEGA=2. DO*PI*FREQ
C          C DELTA=IPHAS*PI/180. DO
C          C NBAUD=1. DO
C          C BAUDD=1. DO/BAUD
C          C MAXY=0. DO
C          C IND2P1=IN/2+1
C          C *** DO THE MODULATION AND ASSIGN THE VALUES TO ARRAY ***
C          C CALL STREAM(DSEED, ANS2, TYPE2, MT)
C          C DO 10 I=1, IN
C          C   ARRAY(R, 1)=AMP*MT*DCOS((OMEGA*TIME)+DELTA)
C          C   ARRAY(R, 2)=TIME
C          C   IF(DABS(ARRAY(R, 1))-GT.MAXY) THEN
C          C     MAXY=DABS(ARRAY(R, 1))
C          C   END IF
C          C   R=R+1
C          C   TIME=TIME+STEP
C          C   IF(TIME-GT.NBAUD*BAUDD) THEN
C          C     CALL STREAM(DSEED, ANS2, TYPE2, MT)
C          C     NBAUD=NBAUD+1. DO
C          C   END IF
C          C CONTINUE
C          C *** PLOT THE TIME SERIES IF DESIRED ***
C          C IF(REP.EQ.1) THEN
C          C   MINY=-MAXY
C          C   CALL PLOT(MAXY, MINY, STEP, IN)
C          C   END IF

```

```

BPS00610
BPS00620
BPS00630
BPS00640
BPS00650
BPS00660
BPS00670
BPS00680
BPS00690
BPS00700
BPS00710
BPS00720
BPS00730
BPS00740
BPS00750
BPS00760
BPS00770
BPS00780
BPS00790
BPS00800
BPS00810
BPS00820
BPS00830
BPS00840
BPS00850
BPS00860
BPS00870
BPS00880
BPS00890
BPS00900
BPS00910
BPS00920
BPS00930
BPS00940
BPS00950
BPS00960
BPS00970
BPS00980
BPS00990
BPS01000
BPS01010
BPS01020
BPS01030
BPS01040
BPS01050
BPS01060
BPS01070
BPS01080
BPS01090
BPS01100

```


C
C
C

C

```
*** ADD THE VALUES OF THE FFT TO THE ACCUMULATED STATISTICS ***  
FLAG=0  
CALL STATS (IN,REP,FLAG)  
RETURN  
END
```

BPS01610
BPS01620
BPS01630
BPS01640
BPS01650
BPS01660
BPS01670
BPS01680

DBP00110
 DBP00120
 DBP00130
 DBP00140
 DBP00150
 DBP00160
 DBP00170
 DBP00180
 DBP00190
 DBP00200
 DBP00210
 DBP00220
 DBP00230
 DBP00240
 DBP00250
 DBP00260
 DBP00270
 DBP00280
 DBP00290
 DBP00300
 DBP00310
 DBP00320
 DBP00330
 DBP00340
 DBP00350
 DBP00360
 DBP00370
 DBP00380
 DBP00390
 DBP00400
 DBP00410
 DBP00420
 DBP00430
 DBP00440
 DBP00450
 DBP00460
 DBP00470
 DBP00480
 DBP00490
 DBP00500
 DBP00510
 DBP00520
 DBP00530
 DBP00540
 DBP00550
 DBP00560
 DBP00570
 DBP00580
 DBP00600

```

SUBROUTINE DBPSK(TYPE2,BAUD,FREQ,IPHAS,AMP,ANS2,
*DSEED,IN,REP)
  *** PURPOSE ***
  THIS SUBROUTINE MODULATES THE CARRIER USING DIFFERENTIAL BINARY
  SHIFT KEYING AS THE MODULATION TECHNIQUE.
  *** PARAMETER DEFINITIONS ***
  TYPE2= INDICATES LOGIC TYPE TO BE EMPLOYED
  BAUD= SYMBOL RATE OR BAUD RATE
  FREQ= CARRIER FREQUENCY
  IPHAS= INITIAL PHASE ANGLE IN DEGREES
  AMP= AMPLITUDE
  ANS2= INTEGER VARIABLE TO BE PASSED TO STREAM GENERATOR
  DSEED= DOUBLE PRECISION SEED FOR RANDOM NUMBER GENERATOR
  IN= NUMBER OF POSITIONS OF ARRAY TO BE UTILIZED
  FLAG= THE CALL THE THIS SUBROUTINE
  AN INTEGER WHICH CONTROL ENTRANCE AND EXIT FROM
  *** VARIABLE DEFINITIONS ***
  ARRAY= A DOUBLE PRECISION ARRAY FOR PASSING THE BINARY
  AND THE FFT
  AND STORING THE VALUE OF THE TIME FUNCTION
  R= AN INTEGER USED TO REPRESENT THE ROW OF ARRAY
  TIME= TIME VARIABLE
  MT= VALUE OF THE BINARY DIGIT
  STEP= INTERVAL AT WHICH THE SIGNAL IS REPRODUCED
  PI= NUMERICAL CONSTANT FREQUENCY
  OMEGA= CARRIER ANGLE IN RADIANS
  DELTA= INITIAL PHASE OF FREQUENCY
  NBAUD= A COUNT OF THE NUMBER OF BAUDS MODULATED
  BAUDD= BAUD DURATION
  REF= REFERENCE VOLTAGE
  BK= VALUE OF DIFFERENTIAL BIT TO BE MODULATED
  X= COMPLEX ARRAY TO RECEIVE THE FFT OF THE TIME SERIES
  IWK= INTEGER ARRAY USED IN SUBROUTINE FFTC
  MAXY= MAXIMUM VALUE TO BE PLOTTED ON THE ABCISSAE
  MINY= MINIMUM VALUE TO BE PLOTTED ON THE ABCISSAE
  RMAX= PRINCIPLE HARMONIC
  REP= AN INTEGER EQUAL TO THE NUMBER OF THE REPETITION OF
  SUBPROGRAM STATS
  IND2P1= LENGTH OF ARRAY DIVIDED BY 2 + 1
  *** VARIABLE DECLARATIONS ***
  INTEGER R,ANS2,TYPE2,IN,EMAX,REP,FLAG,IND2P1
  
```

CC

```

C      DOUBLE PRECISION BAUD, FREQ, IPHAS, AMP, TIME, MT,
*STEP, PI, OMEGA, DELTA, NBAUD, BAUDD,
*DSEED, REF, BK, MAXY, MINY, INT
C      DOUBLE PRECISION ARRAY(1024, 2), SUMX(513), SUMXSQ(513), SUMX3(513),
*SUMX4(513)
C      COMMON ARRAY, SUMX, SUMXSQ, SUMX3, SUMX4
C      COMPLEX*16 X(513)
C      INTEGER IWK(10)
C      *** VARIABLE INITIALIZATION ***
C      R=1
C      TIME=0. DO
C      STEP=1. DO / (2. DO * (FREQ+BAUD))
C      PI=3.141592653589793 DO
C      OMEGA=2. DO * PI * FREQ
C      DELTA=IPHAS * PI / 180. DO
C      NBAUD=1. DO
C      BAUDD=1. DO / BAUD
C      REF=1. DO
C      MAXY=0. DO
C      IND2P1=IN/2+1
C      *** DO THE MODULATION AND ASSIGN THE VALUES TO ARRAY ***
C      CALL STREAM(DSEED, ANS2, TYPE2, MT)
C      BK=REF*MT
C      DO 10 I=1, IN
C      ARRAY(R, 1) = AMP * BK * DCCS((OMEGA*TIME) + DELTA)
C      ARRAY(R, 2) = TIME
C      IF (ARRAY(R, 1) .GT. MAXY) THEN
C      MAXY=ARRAY(R, 1)
C      END IF
C      R=R+1
C      TIME=TIME+STEP
C      IF (TIME .GT. NBAUD * BAUDD) THEN
C      CALL STREAM(DSEED, ANS2, TYPE2, MT)
C      BK=BK*MT
C      NBAUD=NBAUD+1. DO
C      END IF
C      CONTINUE
C      *** ALLOW FOR THE PLOT OF THE TIME SERIES ***
C      IF (REP.EQ.1) THEN

```

```

DBP 00610
DBP 00620
DBP 00630
DBP 00640
DBP 00650
DBP 00660
DBP 00670
DBP 00680
DBP 00690
DBP 00700
DBP 00710
DBP 00720
DBP 00730
DBP 00740
DBP 00750
DBP 00760
DBP 00770
DBP 00780
DBP 00790
DBP 00800
DBP 00810
DBP 00820
DBP 00830
DBP 00840
DBP 00850
DBP 00860
DBP 00870
DBP 00880
DBP 00890
DBP 00900
DBP 00910
DBP 00920
DBP 00930
DBP 00940
DBP 00950
DBP 00960
DBP 00970
DBP 00980
DBP 00990
DBP 01000
DBP 01010
DBP 01020
DBP 01030
DBP 01040
DBP 01050
DBP 01060
DBP 01070
DBP 01080
DBP 01090
DBP 01100

```


DBP01610
DBP01620
DBP01630
DBP01640
DBP01650
DBP01660
DBP01670
DBP01680
DBP01690
DBP01700
DBP01710
DBP01720
DBP01730

```
C      MINY=0. D0  
C      INT=1.D0/STEP  
C      CALL PLOT(MAXY, MINY, INT, IND2P1)  
C      END IF  
C      *** ADD THE VALUES OF THE FFT TO THE ACCUMULATED STATISTICS ***  
C      FLAG=0  
C      CALL STATS(IN, REP, FLAG)  
C      RETURN  
C      END
```



```

10  C
C  C
C  C
C  C
SUM1=SUM1+(MT*(10.DO**KM1))
KM1=KM1-1
CONTINUE
** CONVERT THE REPRESENTATIVE BINARY VARIABLE TO ITS DECIMAL
EQUIVALENT **
SUM2=0.DO
KM1=K-1
ND2=NDP/2.DO
DC 20 I=1,K
IF(SUM1/10.DO**KM1.GE.1.DO) THEN
SUM2=SUM2+ND2
SUM1=SUM1-10.DO**KM1
ND2=ND2/2.DO
KM1=KM1-1
ELSE
ND2=ND2/2.DO
KM1=KM1-1
END IF
CONTINUE
** DO THE MODULATION AND ASSIGN TO ARRAY ***
C=1
FLAG=0
CALL CRTHO(K,MT,SUM2,C,FLAG)
FLAG=2
DO 30 I=1,IN
ARRAY(R,1)=AMP*MT*DCOS((OMEGA*TIME)+DELTA)
ARRAY(R,2)=TIME
IF(ARRAY(R,1).GT.MAXY) THEN
MAXY=ARRAY(R,1)
END IF
R=R+1
TIME=TIME+STEP
IF(TIME.GT.NBIT*BITD) THEN
NBIT=NBIT+1.DO
IF(C.GT.N) THEN
** CONVERT A STREAM OF K BITS TO A SINGLE REPRESENTATIVE BINARY
VARIABLE IN DECIMAL FORM ***
SUM1=0.DO
KM1=K-1
DO 40 J=1,K
CALL STREAM(DSEED,ANS2,TYPE2,MT)
IF(TYPE2.EQ.1.AND.MT.EQ.-1.DO) THEN
MT=0.DO
ELSE IF(TYPE2.EQ.3.AND.MT.EQ.-1.DO) THEN

```

```

OBP01110
OBP01120
OBP01130
OBP01140
OBP01150
OBP01160
OBP01170
OBP01180
OBP01190
OBP01200
OBP01210
OBP01220
OBP01230
OBP01240
OBP01250
OBP01260
OBP01270
OBP01280
OBP01290
OBP01300
OBP01310
OBP01320
OBP01330
OBP01340
OBP01350
OBP01360
OBP01370
OBP01380
OBP01390
OBP01400
OBP01410
OBP01420
OBP01430
OBP01440
OBP01450
OBP01460
OBP01470
OBP01480
OBP01490
OBP01500
OBP01510
OBP01520
OBP01530
OBP01540
OBP01550
OBP01560
OBP01570
OBP01580
OBP01590
OBP01600

```

```

40      MT=1. DO
      END IF
      SUM1=SUM1+(MT*(10. DO**KM1))
      KM1=KM1-1
      CONTINUE
      *** CONVERT THE REPRESENTATIVE BINARY VARIABLE TO ITS DECIMAL
      EQUIVALENT ***
      SUM2=0. DO
      KM1=K-1
      ND2=NDP/2. DO
      DO 50 J=1, K
        IF (SUM1/10. DO**KM1.GE. 1. DO) THEN
          SUM2=SUM2+ND2
          SUM1=SUM1-10. DO**KM1
          ND2=ND2/2. DO
          KM1=KM1-1
        ELSE
          ND2=ND2/2. DO
          KM1=KM1-1
        END IF
      END IF
      CONTINUE
      C=1
      FLAG=1
      END IF
      CALL ORTHO(K, MT, SUM2, C, FLAG)
      FLAG=2
      END IF
      CONTINUE
      *** PLOT THE TIME SERIES IF DESIRED ***
      IF (REP.EQ.1) THEN
        MINY=-MAXY
        CALL PLOT(MAXY, MINY, STEP, IN)
      END IF
      *** GENERATE THE FFT ***
      CALL FFTRC(ARRAY(1,1), IN, X, IWK)
      *** CALCULATE THE AMPLITUDE SPECTRUM OF THE FUNCTION ***
      *** FIND THE NUMBER AND VALUE OF THE PRINCIPLE HARMONIC ***
      N=0. DO
      R=1
      MAXY=0. DO
      DO 60 I=1, IND2P1
      OBP01610
      OBP01620
      OBP01630
      OBP01640
      OBP01650
      OBP01660
      OBP01670
      OBP01680
      OBP01690
      OBP01700
      OBP01710
      OBP01720
      OBP01730
      OBP01740
      OBP01750
      OBP01760
      OBP01770
      OBP01780
      OBP01790
      OBP01800
      OBP01810
      OBP01820
      OBP01830
      OBP01840
      OBP01850
      OBP01860
      OBP01870
      OBP01880
      OBP01890
      OBP01900
      OBP01910
      OBP01920
      OBP01930
      OBP01940
      OBP01950
      OBP01960
      OBP01970
      OBP01980
      OBP01990
      OBP02000
      OBP02010
      OBP02020
      OBP02030
      OBP02040
      OBP02050
      OBP02060
      OBP02070
      OBP02080
      OBP02090
      OBP02100

```



```

60  ARRAY(R,1)=CDABS(X(R))
61  ARRAY(R,2)=N/STEP
62  IF(ARRAY(R,1).GT.MAXY) THEN
63  MAXY=ARRAY(R,1)
64  RMAX=R-1
65  END IF
66  K=R+1
67  N=N+1.D0
68  CONTINUE
69  *** DISPLAY INFO IF THE FIRST TIME THROUGH THE SUBPROGRAM ***
70  IF(REP.EQ.1) THEN
71  WRITE(10,70) RMAX
72  FORMAT(10,70) RMAX
73  *! IS THE FFT HAS BEEN GENERATED! THE PRINCIPLE HARMONIC.
74  *! IS THE 15. HARMONIC. THE NEXT PLOT TO BE PRODUCED WILL.
75  *! BE THE AMPLITUDE SPECTRUM. ENTER A 1 IF YOU ARE READY TO.
76  *! CONTINUE WITH THE PROGRAM.
77  READ(5,*)L
78  IF(L.NE.1) THEN
79  CALL FRICMS('CLRSCRN ')
80  WRITE(10,80)
81  FORMAT('ERROR',/)
82  GO TO 69
83  END IF
84  END IF
85  *** ALLOW FOR THE PLOT OF THE AMPLITUDE SPECTRUM OF THE FFT ***
86  IF(REP.EQ.1) THEN
87  MINY=0.D0
88  INT=1.D0/STEP
89  CALL PLOT(MAXY,MINY,INT,IND2P1)
90  END IF
91  *** ADD THE VALUES OF THE FFT TO THE ACCUMULATED STATISTICS ***
92  FLAG=0
93  CALL STATS(IN,REP,FLAG)
94  RETURN
95  END

```

```

SUBROUTINE QPSK(TYPE2,BAUD,BITS,FREQ,IPHAS,AMP,
*ANS2,DSEED,IN,REP)
*** PURPOSE ***
THIS SUBROUTINE MODULATES THE CARRIER USING QUADRATURE PHASE SHIFT
KEYING AS THE MODULATION TECHNIQUE.
*** PARAMETER DEFINITIONS ***
TYPE2= INDICATES LOGIC TYPE TO BE EMPLOYED
BAUD= SYMBOL RATE OR BAUD RATE
BITS= NUMBER OF BITS IN EACH BINARY CODE WORD
FREQ= CARRIER FREQUENCY
IPHAS= INITIAL PHASE ANGLE IN DEGREES
AMP= AMPLITUDE
ANS2= INTEGER VARIABLE TO BE PASSED TO STREAM GENERATOR
DSEED= DOUBLE PRECISION SEED FOR RANDOM NUMBER GENERATOR
IN= NUMBER OF POSITIONS IN ARRAY TO BE UTILIZED
REP= AN INTEGER EQUAL TO THE NUMBER OF THE REPETITION OF
THE CALL THE THIS SUBROUTINE
*** VARIABLE DEFINITIONS ***
ARRAY= A DOUBLE PRECISION ARRAY FOR PASSING THE BINARY
DIGITS AND STORING THE VALUE OF THE TIME FUNCTION
R= AN INTEGER USED TO REPRESENT THE ROW OF ARRAY
TIME= TIME VARIABLE
MT= VALUE OF BINARY DIGIT PASSED FROM SUBPROGRAM STREAM
MT1= VALUE OF IN-PHASE BINARY DIGIT
MT2= VALUE OF QUADRATURE BINARY DIGIT
STEP= INTERVAL AT WHICH THE SIGNAL IS REPRODUCED
PI= NUMERICAL CONSTANT FREQUENCY
OMEGA= CARRIER ANGULAR FREQUENCY
DELTA= INITIAL PHASE OFFSET IN RADIANS
NBAUD= A COUNT OF THE NUMBER OF BAUDS MODULATED
BAUD= BAUD DURATION
X= COMPLEX ARRAY TO RECEIVE THE FFT OF THE TIME SERIES
IWK= INTEGER WORKING ARRAY USED BY FUNCTION FFTRC
MAXY= MAXIMUM VALUE TO BE PLOTTED ON THE ABCISSAE
MINY= MINIMUM VALUE TO BE PLOTTED ON THE ABCISSAE
INT= INTERVAL BETWEEN POINTS ON THE ORDINATE
RMAG= VALUE OF THE PRINCIPLE HARMONIC
FLAG= AN INTEGER WHICH CONTROL ENTRANCE AND EXIT FROM
SUBPROGRAM STAYS
IND2P1= LENGTH OF ARRAY DIVIDED BY 2 + 1
*** VARIABLE DECLARATIONS ***

```

QPS00110
QPS00120
QPS00130
QPS00140
QPS00150
QPS00160
QPS00170
QPS00180
QPS00190
QPS00200
QPS00210
QPS00220
QPS00230
QPS00240
QPS00250
QPS00260
QPS00270
QPS00280
QPS00290
QPS00300
QPS00310
QPS00320
QPS00330
QPS00340
QPS00350
QPS00360
QPS00370
QPS00380
QPS00390
QPS00400
QPS00410
QPS00420
QPS00430
QPS00440
QPS00450
QPS00460
QPS00470
QPS00480
QPS00490
QPS00500
QPS00510
QPS00520
QPS00530
QPS00540
QPS00550
QPS00560
QPS00570
QPS00580
QPS00590
QPS00600

CC

```

C      INTEGER R,ANS2,TYPE2,IN,RMAX,REP,FLAG,IND2P1
C      DOUBLE PRECISION BAUD,BITS,FREQ,IPHAS,AMP,TIME,MT1,MT2,
C      *STEP,PI,OMEGA,DELTA,NEAUD,BAUDD,
C      *DSEED,MAXY,MINY,INT,MT
C      DOUBLE PRECISION ARRAY(1024,2),SUMX(513),SUMXSQ(513),SUMX3(513),
C      *SUMX4(513)
C      COMMON ARRAY,SUMX,SUMXSQ,SUMX3,SUMX4
C      COMPLEX*16 X(513)
C      INTEGER IWK(10)
C      *** VARIABLE INITIALIZATION ***
C      R=1
C      TIME=0.DO
C      STEP=1.DO/(2.DO*(FREQ+BAUD))
C      PI=3.141592653589793D0
C      OMEGA=2.DO*PI*FREQ
C      DELTA=IPHAS*PI/180.DO
C      NBAUD=1.DO
C      BAUDD=1.DO/BAUD
C      MAXY=0.DO
C      IND2P1=IN/2+1
C      *** DO THE MODULATION AND ASSIGN THE VALUES TO ARRAY***
C      CALL STKRAM(DSEED,ANS2,TYPE2,MT)
C      MT1=MT
C      CALL STREAM(DSEED,ANS2,TYPE2,MT)
C      MT2=MT
C      DO 10 I=1,IN
C      ARRAY(R,1)=AMP*MT1*DCOS((OMEGA*TIME)+DELTA)+
C      * AMP*MT2*DSIN((OMEGA*TIME)+DELTA)
C      ARRAY(R,2)=TIME
C      IF(ARRAY(R,1).GT.MAXY) THEN
C      END IF
C      MAXY=ARRAY(R,1)
C      IF
C      R=R+1
C      TIME=TIME+STEP
C      IF(TIME.GT.NBAUD*BAUDD) THEN
C      CALL STREAM(DSEED,ANS2,TYPE2,MT)
C      MT1=MT
C      CALL STREAM(DSEED,ANS2,TYPE2,MT)
C      MT2=MT
C      NBAUD=NBAUD+1.DO
C      QPS00610
C      QPS00620
C      QPS00630
C      QPS00640
C      QPS00650
C      QPS00660
C      QPS00670
C      QPS00680
C      QPS00690
C      QPS00700
C      QPS00710
C      QPS00720
C      QPS00730
C      QPS00740
C      QPS00750
C      QPS00760
C      QPS00770
C      QPS00780
C      QPS00790
C      QPS00800
C      QPS00810
C      QPS00820
C      QPS00830
C      QPS00840
C      QPS00850
C      QPS00860
C      QPS00870
C      QPS00880
C      QPS00890
C      QPS00900
C      QPS00910
C      QPS00920
C      QPS00930
C      QPS00940
C      QPS00950
C      QPS00960
C      QPS00970
C      QPS00980
C      QPS00990
C      QPS01000
C      QPS01010
C      QPS01020
C      QPS01030
C      QPS01040
C      QPS01050
C      QPS01060
C      QPS01070
C      QPS01080
C      QPS01090
C      QPS01100

```


SUBROUTINE OQPSK(TYPE2, BAUD, BITS, FREQ, IPHAS, AMP,
*ANS2, DSEED, IN, REP)

*** PURPOSE ***

THIS SUBROUTINE MODULATES THE CARRIER USING OFFSET QUADRATURE
PHASE SHIFT KEYING AS THE MODULATION TECHNIQUE.

*** PARAMETER DEFINITIONS ***

TYPE2= INDICATES LOGIC TYPE TO BE EMPLOYED
BAUD= SYMBOL RATE OR BAUD RATE
BITS= NUMBER OF BITS IN EACH BINARY CODE WORD
FREQ= CARRIER FREQUENCY
IPHAS= INITIAL PHASE ANGLE IN DEGREES
AMP= AMPLITUDE
ANS2= INTEGER VARIABLE TO BE PASSED TO STREAM GENERATOR
DSEED= DOUBLE PRECISION SEED FOR RANDOM NUMBER GENERATOR
IN= NUMBER OF POSITIONS IN ARRAY TO BE UTILIZED
REP= AN INTEGER EQUAL TO THE NUMBER OF THE REPETITION OF
THE CALL THE THIS SUBROUTINE

*** VARIABLE DEFINITIONS ***

ARRAY= A DOUBLE PRECISION ARRAY FOR PASSING THE BINARY
AND THE FFT
AND STORING THE VALUE OF THE TIME FUNCTION
AN INTEGER USED TO REPRESENT THE ROW OF ARRAY
TIME= TIME VARIABLE
MT= VALUE OF BINARY DIGIT PASSED FROM SUBPROGRAM STREAM
MT1= VALUE OF IN-PHASE BINARY DIGIT
MT2= VALUE OF QUADRATURE BINARY DIGIT
STEP= INTERVAL AT WHICH THE SIGNAL IS REPRODUCED
PI= NUMERICAL CONSTANT
OMEGA= CARRIER ANGULAR FREQUENCY
DELTA= INITIAL PHASE OFFSET IN RADIAN
NBAUD1= A COUNT OF THE NUMBER OF BAUDS MODULATED IN-PHASE
NBAUD2= COMPLETE ARRAY TO RECEIVE THE FFT OF THE TIME SERIES
X= INTEGER WORKING TO BE PLOTTED ON THE ABCISSAE
IWK= MAXIMUM VALUE TO BE PLOTTED ON THE ORDINATE
MAXY= MINIMUM VALUE BETWEEN POINTS ON THE HARMONIC
MINT= INTERVAL OF THE PRINT CONTROL ENTRANCE AND EXIT FROM
RMAX= AN INTEGER WHICH
FLAG= SUBPROGRAM STATUS
IND2P1= LENGTH OF ARRAY DIVIDED BY 2 + 1

*** VARIABLE DECLARATIONS ***

OQP00110
OQP00120
OQP00130
OQP00140
OQP00150
OQP00160
OQP00170
OQP00180
OQP00190
OQP00200
OQP00210
OQP00220
OQP00230
OQP00240
OQP00250
OQP00260
OQP00270
OQP00280
OQP00290
OQP00300
OQP00310
OQP00320
OQP00330
OQP00340
OQP00350
OQP00360
OQP00370
OQP00380
OQP00390
OQP00400
OQP00410
OQP00420
OQP00430
OQP00440
OQP00450
OQP00460
OQP00470
OQP00480
OQP00490
OQP00500
OQP00510
OQP00520
OQP00530
OQP00540
OQP00550
OQP00560
OQP00570
OQP00580
OQP00590
OQP00600

CC

```

C      INTEGER R,ANS2,TYPE2,IN,EMAX,REP,FLAG,IND2P1
C      DOUBLE PRECISION BAUD,BITS,FREQ,IPHAS,AMP,TIME,MT1,MT2,
C      *STEP,PI,OMEGA,DELTA,BAUDD,NBAUD1,NBAUD2,
C      *DSEED,MAXY,MINY,INT,MT
C      DOUBLE PRECISION ARRAY(1024,2),SUMX(513),SUMXSQ(513),SUMX3(513),
C      *SUMX4(513)
C      COMMON ARRAY,SUMX,SUMXSQ,SUMX3,SUMX4
C      COMPLEX*16 X(513)
C      INTEGER IWK(10)
C      *** VARIABLE INITIALIZATION ***
C      R=1
C      STEP=1.D0/(2.D0*(FREQ+BAUD))
C      PI=3.141592653589793D0
C      OMEGA=2.D0*PI*FREQ
C      DELTA=IPHAS*PI/180.D0
C      NBAUD1=1.D0
C      NBAUD2=1.D0/BAUD
C      BAUDD=1.D0/BAUD
C      TIME=.5D0*BAUDD
C      MAXY=0.D0
C      IND2P1=IN/2+1
C      *** DO THE MODULATION AND ASSIGN THE VALUES TO ARRAY ***
C      CALL STREAM(DSEED,ANS2,TYPE2,MT)
C      MT1=MT
C      CALL STREAM(DSEED,ANS2,TYPE2,MT)
C      MT2=MT
C      DO 10 I=1,IN
C      ARRAY(R,1)=AMP*MT1*DCOS((OMEGA*TIME)+DELTA)+
C      *      AMP*MT2*DSIN((OMEGA*TIME)+DELTA)
C      ARRAY(R,2)=TIME
C      IF(ARRAY(R,1).GT.MAXY) THEN
C      END IF
C      R=R+1
C      TIME=TIME+STEP
C      IF(TIME.GT.NBAUD1*BAUDD) THEN
C      CALL STREAM(DSEED,ANS2,TYPE2,MT)
C      MT1=MT
C      NBAUD1=NBAUD1+1.D0
C      END IF
C      OQP00610
C      OQP00620
C      OQP00630
C      OQP00640
C      OQP00650
C      OQP00660
C      OQP00670
C      OQP00680
C      OQP00690
C      OQP00700
C      OQP00710
C      OQP00720
C      OQP00730
C      OQP00740
C      OQP00750
C      OQP00760
C      OQP00770
C      OQP00780
C      OQP00790
C      OQP00800
C      OQP00810
C      OQP00820
C      OQP00830
C      OQP00840
C      OQP00850
C      OQP00860
C      OQP00870
C      OQP00880
C      OQP00890
C      OQP00900
C      OQP00910
C      OQP00920
C      OQP00930
C      OQP00940
C      OQP00950
C      OQP00960
C      OQP00970
C      OQP00980
C      OQP00990
C      OQP01000
C      OQP01010
C      OQP01020
C      OQP01030
C      OQP01040
C      OQP01050
C      OQP01060
C      OQP01070
C      OQP01080
C      OQP01090
C      OQP01100

```



```

C          CALL FRTCMS('CLRSCRN ')
C          WRITE(10,40)
C          FORMAT(' ERROR',/)
C          GO TO 29
C          END IF
C          END IF
C          *** ALLOW FOR THE PLOT OF THE AMPLITUDE SPECTRUM OF THE FFT ***
C          IF (REP.EQ.1) THEN
C             MINY=0. D0
C             INT=1. D0/STEP
C             CALL PLOT(MAXY,MINY,INT,IND2P1)
C             END IF
C             *** ADD THE VALUES OF THE FFT TO THE ACCUMULATED STATISTICS ***
C             FLAG=0
C             CALL STATS(IN,REP,FLAG)
C             RETURN
C             END

```

```

OQP01610
OQP01620
OQP01630
OQP01640
OQP01650
OQP01660
OQP01670
OQP01680
OQP01690
OQP01700
OQP01710
OQP01720
OQP01730
OQP01740
OQP01750
OQP01760
OQP01770
OQP01780
OQP01790
OQP01800
OQP01810
OQP01820
OQP01830
OQP01840

```

SUBROUTINE MPSK (TYPE2, BAUD, BITS, FREQ, IPHAS, AMP, ANS2,
 *DSEED, IN, REP)

*** PURPOSE ***

THIS SUBROUTINE MODULATES THE CARRIER USING M-ARY PHASE SHIFT
 KEYING AS THE MODULATION TECHNIQUE.

*** PARAMETER DEFINITIONS ***

TYPE2= INDICATES LOGIC TYPE TO BE EMPLOYED
 BAUD= SYMBOL RATE OR BAUD RATE
 BITS= NUMBER OF BITS IN EACH BINARY CODE WORD
 FREQ= CARRIER FREQUENCY
 IPHAS= INITIAL PHASE ANGLE IN DEGREES
 AMP= AMPLITUDE
 ANS2= INTEGER VARIABLE TO BE PASSED TO STREAM GENERATOR
 DSEED= DOUBLE PRECISION SEED FOR RANDOM NUMBER GENERATOR
 IN= NUMBER OF POSITIONS IN ARRAY TO BE UTILIZED
 REP= AN INTEGER EQUAL TO THE NUMBER OF THE REPETITION OF
 THE CALL THE THIS SUBROUTINE

*** VARIABLE DEFINITIONS ***

ARRAY= A DOUBLE PRECISION ARRAY FOR PASSING THE BINARY
 DIGITS AND STORING THE VALUE OF THE TIME FUNCTION
 AND THE FFT USED TO REPRESENT THE ROW OF ARRAY
 TIME= TIME VARIABLE
 MT= VALUE OF THE BINARY DIGIT
 STEP= INTERVAL AT WHICH THE SIGNAL IS REPRODUCED
 PI= NUMERICAL CONSTANT FREQUENCY
 OMEGA= CARRIER ANGULAR OFFSET IN RADIANS
 DELTA= INITIAL PHASE OF THE NUMBER OF BAUDS MODULATED
 BAUD= BAUD DURATION
 X= COMPLEX ARRAY TO RECEIVE THE FFT OF THE TIME SERIES
 LWK= INTEGER WORKING ARRAY USED BY FUNCTION FFTRC
 MAXY= MAXIMUM VALUE TO BE PLOTTED ON THE ABCISSAE
 MINY= MINIMUM VALUE TO BE PLOTTED ON THE ABCISSAE
 INT= INTERVAL BETWEEN POINTS ON THE ORDINATE
 KMAX= VALUE OF THE PRINCIPLE HARMONIC
 K= INTEGER VALUE OF THE NUMBER OF BITS IN A BINARY WORD
 KM1= INTEGER OF POSSIBLE BINARY CODE WORDS = 2**K
 N= NUMBER OF BY
 ND2= N DIVIDED BY 2
 SUM1= VARIABLY USED TO HOLD THE DECIMAL EQUIVALENT TO A
 SUM2= BINARY CODE WORD OF LENGTH K
 J= VARIABLE USED TO HOLD THE DECIMAL CONVERSION OF SUM1
 INTEGER USED TO HOLD THE DECIMAL CONVERSION OF SUM1

MPS00110
 MPS00120
 MPS00130
 MPS00140
 MPS00150
 MPS00160
 MPS00170
 MPS00180
 MPS00190
 MPS00200
 MPS00210
 MPS00220
 MPS00230
 MPS00240
 MPS00250
 MPS00260
 MPS00270
 MPS00280
 MPS00290
 MPS00300
 MPS00310
 MPS00320
 MPS00330
 MPS00340
 MPS00350
 MPS00360
 MPS00370
 MPS00380
 MPS00390
 MPS00400
 MPS00410
 MPS00420
 MPS00430
 MPS00440
 MPS00450
 MPS00460
 MPS00470
 MPS00480
 MPS00490
 MPS00500
 MPS00510
 MPS00520
 MPS00530
 MPS00540
 MPS00550
 MPS00560
 MPS00570
 MPS00580
 MPS00590
 MPS00600

CC


```

10      KM1=KM1-1
      CONTINUE
      *** CONVERT THE REPRESENTATIVE BINARY VARIABLE TO ITS DECIMAL
      EQUIVALENT ***
      SUM2=0. DO
      KM1=K-1
      ND2=N/2. DO
      DO 20 I=1,K
      IF (SUM1/10. DO**KM1.GE.1. DO) THEN
      SUM2=SUM2+ND2
      SUM1=SUM1-10. DO**KM1
      ND2=ND2/2. DO
      KM1=KM1-1
      ELSE
      ND2=ND2/2. DO
      KM1=KM1-1
      END IF
      CONTINUE
      *** DO THE MODULATION AND ASSIGN TO ARRAY ***
      J=R
      DO 30 I=J,IN
      ARRAY(R,1) =AMP*DCOS((OMEGA*TIME)+
      ((SUM2*2. DO*PI)/N)+DELTA)
      ARRAY(R,2) =TIME
      IF (ARRAY(R,1).GT.MAXY) THEN
      MAXY=ARRAY(R,1)
      END IF
      R=R+1
      TIME=TIME+STEP
      IF (TIME.GT.NBAUD*NBAUD) THEN
      NBAUD=NBAUD+1. DO
      GO TO 9
      END IF
      CONTINUE
      END IF
      *** PLOT THE TIME SERIES IF DESIRED ***
      IF (REP.EQ.1) THEN
      MINY=-MAXY
      CALL PLOT(MAXY,MINY,STEP,IN)
      END IF
      *** GENERATE THE FFT ***

```

```

MPS011110
MPS011120
MPS011130
MPS011140
MPS011150
MPS011160
MPS011170
MPS011180
MPS011190
MPS011200
MPS011210
MPS011220
MPS011230
MPS011240
MPS011250
MPS011260
MPS011270
MPS011280
MPS011290
MPS011300
MPS011310
MPS011320
MPS011330
MPS011340
MPS011350
MPS011360
MPS011370
MPS011380
MPS011390
MPS011400
MPS011410
MPS011420
MPS011430
MPS011440
MPS011450
MPS011460
MPS011470
MPS011480
MPS011490
MPS011500
MPS011510
MPS011520
MPS011530
MPS011540
MPS011550
MPS011560
MPS011570
MPS011580
MPS011600

```

```

C      CALL FFTRC(ARRAY(1,1),IN,X,IRK)
C      *** CALCULATE THE AMPLITUDE SPECTRUM OF THE FUNCTION ***
C      *** FIND THE NUMBER AND VALUE OF THE PRINCIPLE HARMONIC ***
N=0. DO
R=1
MAXY=0. DO
DO 4  I=1,IND2P1
ARRAY(R,1)=CDABS(X(R))
ARRAY(R,2)=N/STEP
IF(ARRAY(R,1).GT.MAXY) THEN
MAXY=ARRAY(R,1)
RMAX=R-1
END IF
R=R+1
N=N+1. DO
CONTINUE
*** DISPLAY INFO IF THE FIRST TIME THROUGH THE SUBPROGRAM ***
IF(REP.EQ.1) THEN
WRITE(10,50) RMAX
FORMAT(' THIS FFT HAS BEEN GENERATED! THE PRINCIPLE HARMONIC',
' IS THE ',I5,' HARMONIC. THE NEXT PLOT TO BE PRODUCED WILL',
' BE THE AMPLITUDE SPECTRUM. ENTER A 1 IF YOU ARE READY TO',
' CONTINUE WITH THE PROGRAM.'//,/,)
READ(5,*)L
IF(L.NE.1) THEN
CALL FRTCMS('CLRSCRN ')
WRITE(10,60)
FORMAT(' ERROR',/)
GO TO 49
END IF
END IF
*** ALLOW FOR THE PLOT OF THE AMPLITUDE SPECTRUM OF THE FFT ***
IF(REP.EQ.1) THEN
MINY=0. DO
INT=1. DO/STEP
CALL PLOT(MAXY,MINY,INT,IND2P1)
END IF
*** ADD THE VALUES OF THE FFT TO THE ACCUMULATED STATISTICS ***

```

MPS01610
MPS01620
MPS01630
MPS01640
MPS01650
MPS01660
MPS01670
MPS01680
MPS01690
MPS01700
MPS01710
MPS01720
MPS01730
MPS01740
MPS01750
MPS01760
MPS01770
MPS01780
MPS01790
MPS01800
MPS01810
MPS01820
MPS01830
MPS01840
MPS01850
MPS01860
MPS01870
MPS01880
MPS01890
MPS01900
MPS01910
MPS01920
MPS01930
MPS01940
MPS01950
MPS01960
MPS01970
MPS01980
MPS01990
MPS02000
MPS02010
MPS02020
MPS02030
MPS02040
MPS02050
MPS02060
MPS02070
MPS02080
MPS02090
MPS02100

C

```
FLAG=0  
CALL STATS(IN,REP,FLAG)  
RETURN  
END
```

C

```
MPS02110  
MPS02120  
MPS02130  
MPS02140  
MPS02150  
MPS02160
```

SUBROUTINE MASK (TYPE2, BAUD, BITS, FREQ, IPHAS, AMP, ANS2,
*DSEED, IN, REP)

*** PURPOSE ***

THIS SUBROUTINE MODULATES THE CARRIER USING M-ARY AMPLITUDE SHIFT
KEYING AS THE MODULATION TECHNIQUE.

*** PARAMETER DEFINITIONS ***

TYPE2= INDICATES LOGIC TYPE TO BE EMPLOYED
BAUD= SYMBOL RATE OR BAUD RATE
BITS= NUMBER OF BITS IN EACH BINARY CODE WORD
FREQ= CARRIER FREQUENCY
IPHAS= INITIAL PHASE ANGLE IN DEGREES
AMP= AMPLITUDE
ANS2= INTEGER VARIABLE TO BE PASSED TO STREAM GENERATOR
DSEED= DOUBLE PRECISION SEED FOR RANDOM NUMBER GENERATOR
IN= NUMBER OF POSITIONS IN ARRAY TO BE UTILIZED
FLAG= THE CALL THE THIS SUBROUTINE
AN INTEGER WHICH CONTROL ENTRANCE AND EXIT FROM

*** VARIABLE DEFINITIONS ***

ARRAY= A DOUBLE PRECISION ARRAY FOR PASSING THE BINARY
DIGITS AND STORING THE VALUE OF THE TIME FUNCTION
R= AN INTEGER USED TO REPRESENT THE ROW OF ARRAY
TIME= TIME VARIABLE
MT= VALUE OF THE BINARY DIGIT
STEP= INTERVAL AT WHICH THE SIGNAL IS REPRODUCED
PI= NUMERICAL CONSTANT
OMEGA= CARRIER ANGLE OF FREQUENCY
DELTA= INITIAL PHASE OFFSET IN RADIANS
NBAUD= A COUNT OF THE NUMBER OF BAUDS MODULATED
BAUDD= BAUD DURATION
X= COMPLEX ARRAY TO RECEIVE THE FFT OF THE TIME SERIES
IWK= INTEGER WORKING ARRAY USED BY FUNCTION FFTRC
MAXY= MAXIMUM VALUE TO BE PLOTTED ON THE ABCISSAE
MINT= MINIMUM VALUE TO BE PLOTTED ON THE ABCISSAE
INT= INTERVAL BETWEEN POINTS ON THE ORDINATE
RMAX= VALUE OF THE PRINCIPLE HARMONIC
K= INTEGER VALUE OF THE NUMBER OF BITS IN A BINARY WORD
KM1= INTEGER VALUE OF K MINUS 1
N= NUMBER OF POSSIBLE BINARY CODE WORDS = 2**K
ND2= N DIVIDED BY 2
SUM1= VARIABLE USED TO HOLD THE DECIMAL EQUIVALENT TO A
BINARY CODE WORD OF LENGTH K
SUM2= VARIABLE USED TO HOLD THE DECIMAL CONVERSION OF SUM1
J= INTEGER USED TO INDEX A LOOP

MAS00110
MAS00120
MAS00130
MAS00140
MAS00150
MAS00160
MAS00170
MAS00180
MAS00190
MAS00200
MAS00210
MAS00220
MAS00230
MAS00240
MAS00250
MAS00260
MAS00270
MAS00280
MAS00290
MAS00300
MAS00310
MAS00320
MAS00330
MAS00340
MAS00350
MAS00360
MAS00370
MAS00380
MAS00390
MAS00400
MAS00410
MAS00420
MAS00430
MAS00440
MAS00450
MAS00460
MAS00470
MAS00480
MAS00490
MAS00500
MAS00510
MAS00520
MAS00530
MAS00540
MAS00550
MAS00560
MAS00570
MAS00580
MAS00590
MAS00600

CC

MAS011110
 MAS011120
 MAS011130
 MAS011140
 MAS011150
 MAS011160
 MAS011170
 MAS011180
 MAS011190
 MAS01200
 MAS01210
 MAS01220
 MAS01230
 MAS01240
 MAS01250
 MAS01260
 MAS01270
 MAS01280
 MAS01290
 MAS01300
 MAS01310
 MAS01320
 MAS01330
 MAS01340
 MAS01350
 MAS01360
 MAS01370
 MAS01380
 MAS01390
 MAS01400
 MAS01410
 MAS01420
 MAS01430
 MAS01440
 MAS01450
 MAS01460
 MAS01470
 MAS01480
 MAS01490
 MAS01500
 MAS01510
 MAS01520
 MAS01530
 MAS01540
 MAS01550
 MAS01560
 MAS01570
 MAS01580
 MAS01590
 MAS01600

```

END IF
SUM1=SUM1+(MT*(10.DO**KM1))
KM1=KM1-1
CONTINUE

*** CONVERT THE REPRESENTATIVE BINARY VARIABLE TO ITS DECIMAL
EQUIVALENT ***
SUM2=0. DO
KM1=K-1
ND2=N/2. DO
DO 20 I=1,K
IF (SUM1/10. DO**KM1.GE.1. DO) THEN
SUM2=SUM2+ND2
SUM1=SUM1-10. DO**KM1
ND2=ND2/2. DO
KM1=KM1-1
ELSE
ND2=ND2/2. DO
KM1=KM1-1
END IF
CONTINUE

*** DO THE MODULATION AND ASSIGN TO ARRAY ***
SUM2=SUM2+1. DO
AMP1=AMP/SUM2
J=R
DO 30 I=J,IN
ARRAY(R,2)=AMP1*DCOS((OMEGA*TIME)+DELTA)
ARRAY(R,1)=TIME
IF (ARRAY(R,1).GT.MAXY) THEN
MAXY=ARRAY(R,1)
END IF
R=R+1
TIME=TIME+STEP
IF (TIME.GT.NBAUD*NBAUD) THEN
NBAUD=NBAUD+1. DO
GO TO 9
END IF
CONTINUE

END IF

*** PLOT THE TIME SERIES IF DESIRED ***
IF (REP.EQ.1) THEN
MINY=-MAXY
CALL PLOT(MAXY,MINY,STEP,IN)
END IF

```

10
 C
 C
 C
 C

20
 C
 C
 C

30
 C
 C
 C
 C

MAS02110
MAS02120
MAS02130
MAS02140
MAS02150
MAS02160
MAS02170
MAS02180
MAS02190

END IF
*** ADD THE VALUES OF THE FFT TO THE ACCUMULATED STATISTICS ***
FLAG=0
CALL STATS(IN,REP,FLAG)
RETURN
END

C
C
C
C

QAS001110
 QAS001120
 QAS001130
 QAS001140
 QAS001150
 QAS001160
 QAS001170
 QAS001180
 QAS001190
 QAS00200
 QAS00210
 QAS00220
 QAS00230
 QAS00240
 QAS00250
 QAS00260
 QAS00270
 QAS00280
 QAS00290
 QAS00300
 QAS00310
 QAS00320
 QAS00330
 QAS00340
 QAS00350
 QAS00360
 QAS00370
 QAS00380
 QAS00390
 QAS00400
 QAS00410
 QAS00420
 QAS00430
 QAS00440
 QAS00450
 QAS00460
 QAS00470
 QAS00480
 QAS00490
 QAS00500
 QAS00510
 QAS00520
 QAS00530
 QAS00540
 QAS00550
 QAS00560
 QAS00570
 QAS00580
 QAS00590
 QAS00600

```

SUBROUTINE QASK (TYPE2, BAUD, BITS, FREQ, IPHAS, AMP, ANS2,
*DSEED, IN, REP)
*** PURPOSE ***
THIS SUBROUTINE MODULATES THE CARRIER USING QUADRATURE AMPLITUDE
SHIFT KEYING AS THE MODULATION TECHNIQUE.
*** PARAMETER DEFINITIONS ***
TYPE2= INDICATES LOGIC TYPE TO BE EMPLOYED
BAUD= SYMBOL RATE OR BAUD RATE
BITS= NUMBER OF BITS IN EACH BINARY CODE WORD
FREQ= CARRIER FREQUENCY
IPHAS= INITIAL PHASE ANGLE IN DEGREES
AMP= AMPLITUDE VARIABLE TO BE PASSED TO STREAM GENERATOR
ANS2= INTEGER PRECISION SEED FOR RANDOM NUMBER GENERATOR
DSEED= DOUBLE OF POSITIONS IN ARRAY TO BE UTILIZED
IN= THE CALL THE THIS SUBROUTINE
FLAG= AN INTEGER WHICH CONTROL ENTRANCE AND EXIT FROM
*** VARIABLE DEFINITIONS ***
ARRAY= A DOUBLE PRECISION ARRAY FOR PASSING THE BINARY
DIGITS AND STORING THE VALUE OF THE TIME FUNCTION
AND THE FFT
AN INTEGER USED TO REPRESENT THE ROW OF ARRAY
TIME VARIABLE
VALUE OF THE BINARY DIGIT
INTERVAL AT WHICH THE SIGNAL IS REPRODUCED
NUMERICAL CONSTANT FREQUENCY
CARRIER ANGLE OFFSET IN RADIANS
INITIAL PHASE OF THE NUMBER OF BAUDS MODULATED
A BOUND DURATION
COMPLEX ARRAY TO RECEIVE THE FFT OF THE TIME SERIES
INTEGER WORKING ARRAY USED BY FUNCTION FFTRC
MAXIMUM VALUE TO BE PLOTTED ON THE ABCISSAE
MINIMUM VALUE TO BE PLOTTED ON THE ABCISSAE
INTERVAL BETWEEN POINTS ON THE ORDINATE
VALUE OF THE PRINCIPLE HARMONIC
INTEGER VALUE OF K MINUS 1
NUMBER OF POSSIBLE BINARY CODE WORDS = 2**K
N DIVIDED BY 2
VARIABLE USED TO HOLD THE DECIMAL EQUIVALENT TO A
BINARY CODE WORD OF LENGTH K
INTEGER USED TO HOLD THE DECIMAL CONVERSION OF SUM1
INTEGER USED TO INDEX A LOOP
  
```

CC

MSK00110
MSK00120
MSK00130
MSK00140
MSK00150
MSK00160
MSK00170
MSK00180
MSK00190
MSK00200
MSK00210
MSK00220
MSK00230
MSK00240
MSK00250
MSK00260
MSK00270
MSK00280
MSK00290
MSK00300
MSK00310
MSK00320
MSK00330
MSK00340
MSK00350
MSK00360
MSK00370
MSK00380
MSK00390
MSK00400
MSK00410
MSK00420
MSK00430
MSK00440
MSK00450
MSK00460
MSK00470
MSK00480
MSK00490
MSK00500
MSK00510
MSK00520
MSK00530
MSK00540
MSK00550
MSK00560
MSK00570
MSK00580
MSK00590
MSK00600

```
SUBROUTINE MSK(TYPE2, BAUD, FREQ, IPHAS, AMP, ANS2,  
*DSEED, IN, REP)  
*** PURPOSE ***  
THIS SUBROUTINE MODULATES THE CARRIER USING MINIMUM SHIFT KEYING  
OR FAST FREQUENCY SHIFT KEYING AS THE MODULATION TECHNIQUE.  
*** PARAMETER DEFINITIONS ***  
TYPE2= INDICATES LOGIC TYPE TO BE EMPLOYED  
BAUD= SYMBOL RATE OR BAUD RATE  
FREQ= CARRIER FREQUENCY  
IPHAS= INITIAL PHASE ANGLE IN DEGREES  
AMP= AMPLITUDE  
ANS2= INTEGER VARIABLE TO BE PASSED TO STREAM  
DSEED= DOUBLE PRECISION SEED FOR RANDOM NUMBER GENERATOR  
IN= NUMBER OF POSITIONS IN ARRAY TO BE UTILIZED  
REP= AN INTEGER EQUAL TO THE NUMBER OF THE REPETITION OF  
THE CALL THE THIS SUBROUTINE  
*** VARIABLE DEFINITIONS ***  
ARRAY= A DOUBLE PRECISION ARRAY FOR PASSING THE BINARY  
DIGITS AND STORING THE VALUE OF THE TIME FUNCTION  
R= AN INTEGER USED TO REPRESENT THE ROW OF ARRAY  
TIME= TIME VARIABLE  
STEP= VALUE OF THE BINARY DIGIT  
PI= INTERVAL AT WHICH THE SIGNAL IS REPRODUCED  
OMEGA= CARRIER ANGULAR FREQUENCY  
DELTA= INITIAL PHASE OFFSET IN RADIAN  
NBAUD= A COUNT OF THE NUMBER OF BAUDS MODULATED  
BAUDD= BAUD DURATION  
X= COMPLEX ARRAY TO RECEIVE THE FFT OF THE TIME SERIES  
IWK= INTEGER WORKING ARRAY USED BY FUNCTION FFTRC  
MAXY= MAXIMUM VALUE TO BE PLOTTED ON THE ABCISSAE  
MINT= MINIMUM VALUE TO BE PLOTTED ON THE ABCISSAE  
INT= INTERVAL BETWEEN POINTS ON THE ORDINATE  
RMAX= VALUE OF THE PRINCIPLE HARMONIC  
FLAG= AN INTEGER WHICH CONTROL ENTRANCE AND EXIT FROM  
SUBPROGRAM STATS  
IND2P1= LENGTH OF ARRAY DIVIDED BY 2 + 1  
*** VARIABLE DECLARATIONS ***  
INTEGER R, ANS2, TYPE2, IN, RMAX, REP, FLAG, IND2P1  
DOUBLE PRECISION BAUD, FREQ, IPHAS, AMP, TIME, MT,
```

CC

```

C      *STEP,PI,OMEGA,DELTA,NBAUD,BAUDD,
C      *DSEED,MAXY,MINY,INT
C      DOUBLE PRECISION ARRAY(1024,2),SUMX(513),SUMXSQ(513),SUMX3(513),
C      *SUMX4(513)
C      COMMON ARRAY,SUMX,SUMXSQ,SUMX3,SUMX4
C      COMPLEX*16 X(513)
C      INTEGER IWK(10)
C      *** VARIABLE INITIALIZATION ***
C      R=1
C      TIME=0.D0
C      STEP=1.D0/(2.D0*(FREQ+(1.25D0*BAUD)))
C      PI=3.141592653589793D0
C      OMEGA=2.D0*PI*FREQ
C      DELTA=IPHAS*PI/180.D0
C      NBAUD=1.D0
C      BAUDD=1.D0/BAUD
C      MAXY=0.D0
C      IND2P1=IN/2+1
C      CALL STREAM(DSEED,ANS2,TYPE2,MT)
C
C      DO 10 I=1,IN
C      ARRAY(R,1)=AMP*DCOS(((OMEGA+((MT*PI)/(2.D0*BAUDD))))*TIME)
C      +DELTA
C      ARRAY(R,2)=TIME
C      IF(DABS(ARRAY(R,1)).GT.MAXY) THEN
C      MAXY=DABS(ARRAY(R,1))
C      END IF
C      R=R+1
C      TIME=TIME+STEP
C      IF(TIME.GT.NBAUD*BAUDD) THEN
C      CALL STREAM(DSEED,ANS2,TYPE2,MT)
C      NBAUD=NBAUD+1.D0
C      END IF
C      CONTINUE
C      *** PLOT THE TIME SERIES IF DESIRED ***
C      IF(R.EQ.1) THEN
C      MINY=-MAXY
C      CALL PLOT(MAXY,MINY,STEP,IN)
C      END IF
C      *** GENERATE THE FFT ***

```

```

MSK 00610
MSK 00620
MSK 00630
MSK 00640
MSK 00650
MSK 00660
MSK 00670
MSK 00680
MSK 00690
MSK 00700
MSK 00710
MSK 00720
MSK 00730
MSK 00740
MSK 00750
MSK 00760
MSK 00770
MSK 00780
MSK 00790
MSK 00800
MSK 00810
MSK 00820
MSK 00830
MSK 00840
MSK 00850
MSK 00860
MSK 00870
MSK 00880
MSK 00890
MSK 00900
MSK 00910
MSK 00920
MSK 00930
MSK 00940
MSK 00950
MSK 00960
MSK 00970
MSK 00980
MSK 00990
MSK 01000
MSK 01010
MSK 01020
MSK 01030
MSK 01040
MSK 01050
MSK 01060
MSK 01070
MSK 01080
MSK 01090
MSK 01100

```

MSK01110
 MSK01120
 MSK01130
 MSK01140
 MSK01150
 MSK01160
 MSK01170
 MSK01180
 MSK01190
 MSK01200
 MSK01210
 MSK01220
 MSK01230
 MSK01240
 MSK01250
 MSK01260
 MSK01270
 MSK01280
 MSK01290
 MSK01300
 MSK01310
 MSK01320
 MSK01330
 MSK01340
 MSK01350
 MSK01360
 MSK01370
 MSK01380
 MSK01390
 MSK01400
 MSK01410
 MSK01420
 MSK01430
 MSK01440
 MSK01450
 MSK01460
 MSK01470
 MSK01480
 MSK01490
 MSK01500
 MSK01510
 MSK01520
 MSK01530
 MSK01540
 MSK01550
 MSK01560
 MSK01570
 MSK01580
 MSK01600

```

C      CALL FFTRC(ARRAY(1,1),IN,X,IWK)
C
C      *** CALCULATE THE AMPLITUDE SPECTRUM OF THE FUNCTION ***
C      *** FIND THE NUMBER AND VALUE OF THE PRINCIPLE HARMONIC ***
C
C      N=0. DO
C      R=1
C      MAXY=0. DO
C      DO 20 I=1,IND2P1
C      ARRAY(R,1)=CDABS(X(R))
C      ARRAY(R,2)=N/STEP
C      IF(ARRAY(R,1).GT.MAXY) THEN
C      MAXY=ARRAY(R,1)
C      RMAX=R-1
C      END IF
C      R=R+1
C      N=N+1. DO
C      CONTINUE
C
C      *** DISPLAY INFO IF THE FIRST TIME THROUGH SUBPROGRAM ***
C      IF(REP.EQ.1) THEN
C      WRITE(10,30)RMAX
C      FORMAT(1,30)
C      *! IS THE AMPLITUDE SPECTRUM. ENTER A 1 IF YOU ARE READY TO
C      *! BE THE HARMONIC. THE NEXT PLOT TO BE PRODUCED WILL
C      *! CONTINUE WITH THE PROGRAM. //:
C      READ(5,*)L
C      IF(L.NE.1) THEN
C      CALL FRTCMS('CLRSCRN ')
C      WRITE(10,40)
C      FORMAT(1,40)
C      GO TO 9
C      END IF
C      END IF
C
C      *** ALLOW FOR THE PLOT OF THE AMPLITUDE SPECTRUM OF THE FFT ***
C      IF(REP.EQ.1) THEN
C      MINY=0. DO
C      INT=1. DO/STEP
C      CALL PLOT(MAXY,MINY,INT,IND2P1)
C      END IF
  
```

MSK01610
MSK01620
MSK01630
MSK01640
MSK01650
MSK01660
MSK01670

*** ADD THE VALUES OF THE FFT TO THE ACCUMULATED STATISTICS ***

FLAG=0
CALL STATS(IN,REP,FLAG)
RETURN
END

C
C
C

MFS00110
MFS00120
MFS00130
MFS00140
MFS00150
MFS00160
MFS00170
MFS00180
MFS00190
MFS00200
MFS00210
MFS00220
MFS00230
MFS00240
MFS00250
MFS00260
MFS00270
MFS00280
MFS00290
MFS00300
MFS00310
MFS00320
MFS00330
MFS00340
MFS00350
MFS00360
MFS00370
MFS00380
MFS00390
MFS00400
MFS00410
MFS00420
MFS00430
MFS00440
MFS00450
MFS00460
MFS00470
MFS00480
MFS00490
MFS00500
MFS00510
MFS00520
MFS00530
MFS00540
MFS00550
MFS00560
MFS00570
MFS00580
MFS00590
MFS00600

```

SUBROUTINE MFSK (TYPE2, BAUD, BITS, FREQ, IPHAS, AMP, ANS2,
* DSEED, IN, REP)
*** PURPOSE ***
THIS SUBROUTINE MODULATES THE CARRIER USING M-ARY FREQUENCY SHIFT
KEYING AS THE MODULATION TECHNIQUE.
*** PARAMETER DEFINITIONS ***
TYPE2= INDICATES LOGIC TYPE TO BE EMPLOYED
BAUD= SYMBOL RATE OR BAUD RATE
BITS= NUMBER OF BITS IN EACH BINARY CODE WORD
FREQ= CARRIER FREQUENCY
IPHAS= INITIAL PHASE ANGLE IN DEGREES
AMP= AMPLITUDE
ANS2= INTEGER VARIABLE TO BE PASSED TO STREAM GENERATOR
DSEED= DOUBLE PRECISION SEED FOR RANDOM NUMBER UTILIZED
IN= NUMBER OF POSITIONS IN ARRAY TO BE UTILIZED
REP= AN INTEGER EQUAL TO THE NUMBER OF THE REPETITION OF
THE CALL THIS SUBROUTINE
*** VARIABLE DEFINITIONS ***
ARRAY= A DOUBLE PRECISION ARRAY FOR PASSING THE BINARY
DIGITS AND STORING THE VALUE OF THE TIME FUNCTION
R= AN INTEGER USED TO REPRESENT THE ROW OF ARRAY
TIME= TIME VARIABLE
MT= VALUE OF THE BINARY DIGIT
STEP= INTERVAL AT WHICH THE SIGNAL IS REPRODUCED
PI= NUMERICAL CONSTANT
OMEGA= CARRIER ANGLE OFFSET IN RADIANS
DELTA= INITIAL PHASE OF THE NUMBER OF BAUDS MODULATED
NBAUD= A COUNT OF THE NUMBER OF BAUDS MODULATED
BAUDD= BAUD DURATION
X= COMPLEX ARRAY TO RECEIVE THE FFT OF THE TIME SERIES
IWK= INTEGER WORKING ARRAY USED BY FUNCTION FFTRC
MAXY= MAXIMUM VALUE TO BE PLOTTED ON THE ABCISSAE
MINY= MINIMUM VALUE TO BE PLOTTED ON THE ABCISSAE
INT= INTERVAL BETWEEN POINTS ON THE ORDINATE
RMAX= VALUE OF THE PRINCIPLE HARMONIC
K= INTEGER VALUE OF THE NUMBER OF BITS IN A BINARY WORD
KM1= INTEGER VALUE OF K MINUS 1
N= NUMBER OF POSSIBLE BINARY CODE WORDS = 2**K
ND2= N DIVIDED BY 2
SUM1= VARIABLE USED TO HOLD THE DECIMAL EQUIVALENT TO A
BINARY CODE WORD OF LENGTH K
SUM2= VARIABLE USED TO HOLD THE DECIMAL CONVERSION OF SUM1
J= INTEGER USED TO INDEX A LOOP

```

CC


```

DO 10 I=1,K
CALL STREAM(DSEED,ANS2,TYPE2,MT)
IF (TYPE2.EQ.1.AND.MT.EQ.-1.D0) THEN
ELSE IF (TYPE2.EQ.3.AND.MT.EQ.-1.D0) THEN
MT=1.D0
END IF
SUM 1=SUM 1+(MT*(10.D0**KM1))
KM1=KM1-1
CONTINUE

*** CONVERT THE REPRESENTATIVE BINARY VARIABLE TO ITS DECIMAL
EQUIVALENT ***
SUM 2=0.D0
KM1=K-1
ND 2=N/2.D0
DO 20 I=1,K
IF (SUM 1/10.D0**KM1.GE.1.D0) THEN
SUM 2=SUM 2+ND 2
SUM 1=SUM 1-10.D0**KM 1
ND 2=ND 2/2.D0
KM 1=KM 1-1
ELSE
ND 2=ND 2/2.D0
KM 1=KM 1-1
END IF
CONTINUE

*** DO THE MODULATION AND ASSIGN TO ARRAY ***
J=R
MFR EQ=-FRNGD 2+(SUM 2*DELF)
DO 30 I=J,IN
ARRAY(R,1)=AMP*DCOS(((OMEGA+(2.D0*PI*M FREQ))*TIME)+
DELTA)
ARRAY(R,2)=TIME
IF (ARRAY(R,1).GT.MAXY) THEN
MAXY=ARRAY(R,1)
END IF
R=R+1
TIME=TIME+STEP
IF (TIME.GT.NBAUD*BAUDD) THEN
NBAUD=NBAUD+1.D0
GO TO 9
END IF
CONTINUE
END IF

*** PLOT THE TIME SERIES IF DESIRED ***

```

10
C
C
C
C

20
C
C
C

30
C
C

MFS 01110
MFS 01120
MFS 01130
MFS 01140
MFS 01150
MFS 01160
MFS 01170
MFS 01180
MFS 01190
MFS 01200
MFS 01210
MFS 01220
MFS 01230
MFS 01240
MFS 01250
MFS 01260
MFS 01270
MFS 01280
MFS 01290
MFS 01300
MFS 01310
MFS 01320
MFS 01330
MFS 01340
MFS 01350
MFS 01360
MFS 01370
MFS 01380
MFS 01390
MFS 01400
MFS 01410
MFS 01420
MFS 01430
MFS 01440
MFS 01450
MFS 01460
MFS 01470
MFS 01480
MFS 01490
MFS 01500
MFS 01510
MFS 01520
MFS 01530
MFS 01540
MFS 01550
MFS 01560
MFS 01570
MFS 01580
MFS 01590
MFS 01600

```

C      IF (REP.EQ.1) THEN
C      MINY=-MAXY
C      CALL PLOT(MAXY,MINY,STEP,IN)
C      END IF
C      *** GENERATE THE FFT ***
C      CALL FFTRC(ARRAY(1,1),IN,X,IWK)
C      *** CALCULATE THE AMPLITUDE SPECTRUM OF THE FUNCTION ***
C      *** FIND THE NUMBER AND VALUE OF THE PRINCIPLE HARMONIC ***
C      N=0.DO
C      R=1
C      MAXY=0.DO
C      DO 40 I=1,IND2P1
C      ARRAY(R,1)=CDABS(X(R))
C      ARRAY(R,2)=N/STEP
C      IF (ARRAY(R,1).GT.MAXY) THEN
C      MAXY=ARRAY(R,1)
C      RMAX=R-1
C      END IF
C      R=R+1
C      N=N+1.DO
C      CONTINUE
C      *** DISPLAY INFO IF THE FIRST TIME THROUGH THE SUBPROGRAM ***
C      IF (REP.EQ.1) THEN
C      WRITE(10,50) RMAX
C      FORMAT(10,50) THE FFT HAS BEEN GENERATED! THE PRINCIPLE HARMONIC
C      * IS THE 15 HARMONIC. THE NEXT PLOT TO BE PRODUCED WILL
C      * BE THE AMPLITUDE SPECTRUM. ENTER A 1 IF YOU ARE READY TO
C      * CONTINUE WITH THE PROGRAM.//:/:/
C      READ(5,*)L
C      IF(L.NE.1) THEN
C      CALL FRTCMS('CLRSCRN ')
C      WRITE(10,60)
C      FORMAT('ERROR',/)
C      GO TO 49
C      END IF
C      END IF
C      *** ALLOW FOR THE PLOT OF THE AMPLITUDE SPECTRUM OF THE FFT ***

```

```

MFS01610
MFS01620
MFS01630
MFS01640
MFS01650
MFS01660
MFS01670
MFS01680
MFS01690
MFS01700
MFS01710
MFS01720
MFS01730
MFS01740
MFS01750
MFS01760
MFS01770
MFS01780
MFS01790
MFS01800
MFS01810
MFS01820
MFS01830
MFS01840
MFS01850
MFS01860
MFS01870
MFS01880
MFS01890
MFS01900
MFS01910
MFS01920
MFS01930
MFS01940
MFS01950
MFS01960
MFS01970
MFS01980
MFS01990
MFS02000
MFS02010
MFS02020
MFS02030
MFS02040
MFS02050
MFS02060
MFS02070
MFS02080
MFS02090
MFS02100

```



```
C      IF (REP.EQ.1) THEN
C      MINY=0.D0
C      INT=1.D0/STEP
C      CALL PLOT(MAXY, MINY, INT, IND2P1)
C      END IF
C      FLAG=0
C      CALL STATS(IN, REP, FLAG)
C      RETURN
C      END
```

```
MFS02110
MFS02120
MFS02130
MFS02140
MFS02150
MFS02160
MFS02170
MFS02180
MFS02190
MFS02200
MFS02210
MFS02220
MFS02230
```

```

SUBROUTINE QPRS (TYPE2, TYPE3, BAUD, BITS, FREQ, IPHAS, AMP,
*ANS2, DSEED, IN, REP)
*** PURPOSE ***
THIS SUBROUTINE MODULATES THE CARRIER USING QUADRATURE PHASE SHIFT
KEYING AS THE MODULATION TECHNIQUE.
*** PARAMETER DEFINITIONS ***
TYPE2= INDICATES LOGIC TYPE TO BE EMPLOYED
TYPE3= INDICATES THE CLASS OF QPRS
BAUD= SYMBOL RATE OR BAUD RATE
BITS= NUMBER OF BITS IN EACH BINARY CODE WORD
FREQ= CARRIER FREQUENCY
IPHAS= INITIAL PHASE ANGLE IN DEGREES
AMP= AMPLITUDE
ANS2= INTEGER VARIABLE TO BE PASSED TO STREAM GENERATOR
DSEED= DOUBLE PRECISION SEED FOR RANDOM NUMBER GENERATOR
IN= NUMBER OF POSITIONS IN ARRAY TO BE UTILIZED
REP= AN INTEGER EQUAL TO THE NUMBER OF THE REPEITION OF
THE CALL THE THIS SUBROUTINE
*** VARIABLE DEFINITIONS ***
AREAY= A DOUBLE PRECISION ARRAY FOR PASSING THE BINARY
AND THE STORING THE VALUE OF THE TIME FUNCTION
ASUBN= A DOUBLE PRECISION ARRAY CONTAINING THE VALUES OF
THE IN PHASE BINARY DIGIT TO BE MODULATED
BSUBN= A DOUBLE PRECISION ARRAY CONTAINING THE VALUES OF THE
QUADRATURE BINARY DIGIT TO BE MODULATED
HOFT= THE IMPULSE RESPONSE FOR THE SPECIFIED CLASS FILTER
T= VARIABLE WHICH DETERMINES THE MAGNITUDE OF THE IMPULSE
NDP= VARIABLE USED FOR A SPECIFIED BINARY DIGIT
R= AN INTEGER USED IN THE COMPUTATION OF T
TIME= TIME VARIABLE
MT= VALUE OF BINARY DIGIT PASSED FROM SUBPROGRAM STREAM
STEP= INTERVAL AT WHICH THE SIGNAL IS REPRODUCED
PI= NUMERICAL CONSTANT
OMEGA= CARRIER ANGLE OFFSET IN RADIANS
DELTA= INITIAL PHASE AND QPRS BIT DURATION OF THE TIME SERIES
BAUDD= COMPLEX WORKING TO RECEIVE BY FUNCTION FFTRC
X= BAUD DURATION TO BE PLOTTED ON THE ABCISSAE
IWK= MAXIMUM VALUE TO BE PLOTS ON THE ORDINATE
MXY= MINIMUM VALUE BETWEEN POINTS ON THE HARMONIC
MINT= INTERVAL OF THE PRINCIPLE HARMONIC
RMAX= VALUE OF THE PRINCIPLE HARMONIC

```

```

QPR00110
QPR00120
QPR00130
QPR00140
QPR00150
QPR00160
QPR00170
QPR00180
QPR00190
QPR00200
QPR00210
QPR00220
QPR00230
QPR00240
QPR00250
QPR00260
QPR00270
QPR00280
QPR00290
QPR00300
QPR00310
QPR00320
QPR00330
QPR00340
QPR00350
QPR00360
QPR00370
QPR00380
QPR00390
QPR00400
QPR00410
QPR00420
QPR00430
QPR00440
QPR00450
QPR00460
QPR00470
QPR00480
QPR00490
QPR00500
QPR00510
QPR00520
QPR00530
QPR00540
QPR00550
QPR00560
QPR00570
QPR00580
QPR00590
QPR00600

```

CC

C

```

DO 40 J=1, INDEX
NDP=J-1
T=TIME-(NDP/BAUD)
IF(TYPE3.EQ.1) THEN
IF(T.EQ.-BAUDD/2.D0.OR.T.EQ.BAUDD/2.D0) THEN
HFFT=1.D0
ELSE
HFFT= (4.D0/(BAUD**2*PI)) * (DCOS(PI*T*BAUD) /
((1.D0/BAUD**2) - (4.D0*T**2)))
END IF
ELSE IF (TYPE3.EQ.2) THEN
IF(T.EQ.0.D0) THEN
HFFT=2.D0
ELSE IF (T.EQ.-BAUDD.OR.T.EQ.BAUDD) THEN
HFFT=1.D0
ELSE
HFFT= (2.D0/(BAUD**3*PI*T)) * (DSIN(PI*T*BAUD) /
((1.D0/BAUD**2) - T**2))
END IF
ELSE IF (TYPE3.EQ.3) THEN
IF(T.EQ.0.D0) THEN
HFFT=1.D0
ELSE IF (T.EQ.-BAUDD) THEN
HFFT=2.D0
ELSE IF (T.EQ.BAUDD) THEN
HFFT=-1.D0
ELSE
HFFT= (1.D0/(BAUD**2*PI*T)) * (DSIN(PI*T*BAUD) *
((3.D0*T-BAUDD)/(T**2 - (1.D0/BAUD**2))))
END IF
ELSE IF (TYPE3.EQ.4) THEN
IF(T.EQ.-BAUDD) THEN
HFFT=1.D0
ELSE IF (T.EQ.BAUDD) THEN
HFFT=-1.D0
ELSE
HFFT= (2.D0/(BAUD**2*PI)) * (DSIN(PI*T*BAUD) /
(T**2 - (1.D0/BAUD**2)))
END IF
ELSE IF (TYPE3.EQ.5) THEN
IF(T.EQ.0.D0) THEN
HFFT=-2.D0
ELSE IF (T.EQ.-2.D0*BAUDD.OR.T.EQ.2.D0*BAUDD) THEN
HFFT=1.D0
ELSE
HFFT= (8.D0/(BAUD**3*PI*T)) * (DSIN(PI*T*BAUD) /
(T**2 - (4.D0/BAUD**2)))
END IF

```

C

```

QPR01110
QPR01120
QPR01130
QPR01140
QPR01150
QPR01160
QPR01170
QPR01180
QPR01190
QPR01200
QPR01210
QPR01220
QPR01230
QPR01240
QPR01250
QPR01260
QPR01270
QPR01280
QPR01290
QPR01300
QPR01310
QPR01320
QPR01330
QPR01340
QPR01350
QPR01360
QPR01370
QPR01380
QPR01390
QPR01400
QPR01410
QPR01420
QPR01430
QPR01440
QPR01450
QPR01460
QPR01470
QPR01480
QPR01490
QPR01500
QPR01510
QPR01520
QPR01530
QPR01540
QPR01550
QPR01560
QPR01570
QPR01580
QPR01590
QPR01600

```



```

59 WRITE(10,60) RMAX
60 FORMAT(' THE FFT HAS BEEN GENERATED! THE PRINCIPLE HARMONIC', //
        '* IS THE 15. HARMONIC. THE NEXT PLOT TO BE PRODUCED WILL', //
        '* BE THE AMPLITUDE SPECTRUM. ENTER A 1 IF YOU ARE READY TO', //
        '* CONTINUE WITH THE PROGRAM.', //, //)
C READ(5,*) L
C IF(L.NE.1) THEN
C CALL FKTCMS('CLRSCRN ')
70 WRITE(10,70)
C FORMAT(' ERROR', //)
C GO TO 59
C END IF
C END IF
C *** ALLOW FOR THE PLOT OF THE AMPLITUDE SPECTRUM OF THE FFT ***
C IF(REP.EQ.1) THEN
C MINY=0. DO
C INT=1. DO/STEP
C CALL PLOT(MAXY, MINY, INT, IND2P1)
C END IF
C *** ADD THE VALUES OF THE FFT TO THE ACCUMULATED STATISTICS ***
C FLAG=0
C CALL STATS(IN, REP, FLAG)
C RETURN
C END

```

```

QPR 021110
QPR 021120
QPR 021130
QPR 021140
QPR 021150
QPR 021160
QPR 021170
QPR 021180
QPR 021190
QPR 022000
QPR 022100
QPR 022200
QPR 022300
QPR 022400
QPR 022500
QPR 022600
QPR 022700
QPR 022800
QPR 022900
QPR 023000
QPR 023100
QPR 023200
QPR 023300
QPR 023400
QPR 023500
QPR 023600
QPR 023700
QPR 023800
QPR 023900
QPR 024000
QPR 024100
QPR 024200
QPR 024300

```


MT= I MT
END IF
RETURN
END

STR 00610
STR 00620
STR 00630
STR 00640


```

SUBROUTINE ORTHO (K, MT, SUM2, C, FLAG)
*** PURPOSE ***
THIS SUBROUTINE GENERATES AN ORTHOGONAL SET OF N VECTORS OF LENGTH
N WHERE N IS 2**K, WHERE K IS THE LENGTH OF THE BINARY CODE WORD.
AND DETERMINES THE VALUE, MT, OF A BINARY DIGIT TO BE RETURNED
*** PARAMETER DEFINITIONS ***
K=      NUMBER OF BITS IN THE BINARY CODE WORD
MT=     THE VALUE OF THE BINARY DIGIT TO BE MODULATED
SUM2=   THE DECIMAL EQUIVALENT OF A SET OF RANDOMLY DRAWN
        BINARY DIGITS
C=      THE COLUMN OF THE VECTOR WHERE THE BINARY DIGIT TO
        BE MODULATED IS LOCATED
FLAG=   INTEGER WHICH CONTROLS POINT OF ENTRY TO SUBROUTINE
        CRTHO
*** VARIABLE DEFINITIONS ***
ROW=    RCW OF ARRAY H2N WHICH MATCHES A BINARY CODE WORD
KM1=    INTEGER VALUE OF K MINUS 1
N=      NUMBER OF POSSIBLE BINARY CODE WORDS = 2**K
H2N=    MATRIX OF N ORTHOGONAL VECTORS OF LENGTH N
RH2N=   ROW OF MATRIX H2N
CH2N=   COLUMN OF MATRIX H2N
RH2NP1= RANK OF MATRIX H2N EQUAL TO HALF THE RANK PLUS 1
CH2NP1= COLUMN OF MATRIX H2N EQUAL TO HALF THE RANK PLUS 1
X=      DOUBLE PRECISION EQUIVALENT ROW REPRESENTATION OF H2N
*** VARIABLE DECLARATIONS ***
INTEGER K, RH2N, CH2N, RH2NP1, CH2NP1, H2NR, N, KM1, H2N(65,65),
*FLAG, ROW, C
DOUBLE PRECISION X, MT, SUM2
*** VARIABLE INITIALIZATION ***
KM1=K-1
N=2**K
RH2N=1
CH2N=1
H2NR=2
EH2NP1=H2NR+1
CH2NP1=H2NR+1
H2N(1,1)=1
H2N(1,2)=1

```

CC

```

C C C
H2N {2,1} = 1
H2N {2,2} = -1
*** GENERATE A MATRIX OF N ORTHOGONAL VECTORS OF LENGTH N ***
IF (FLAG.EQ.0) THEN
DO 10 I=1, KM1
DO 20 L=1, H2NR
DO 30 M=1, H2NR
H2N (RH2N, CH2N) = H2N (RH2N, CH2N)
H2N (RH2N, CH2NP1) = H2N (RH2N, CH2N)
H2N (RH2NP1, CH2N) = H2N (RH2N, CH2N)
H2N (RH2NP1, CH2NP1) = -H2N (RH2N, CH2N)
CH2N = CH2N + 1
CH2NP1 = CH2NP1 + 1
CONTINUE
RH2N = RH2N + 1
RH2NP1 = RH2NP1 + 1
CH2N = 1
CH2NP1 = H2NR + 1
CONTINUE
H2NR = 2 * H2NR
RH2N = 1
CH2N = 1
RH2NP1 = H2NR + 1
CH2NP1 = H2NR + 1
CONTINUE
*** ASSIGN EACH ROW OF H2N A REPRESENTATIVE DECIMAL NUMBER ***
DO 40 I=1, N
H2N (I, 65) = I - 1
CONTINUE
*** DETERMINE WHICH ROW OR H2N MATCHES THE VALUE OF THE
REPRESENTATIVE DECIMAL EQUIVALENT TO THE BINARY CODE WORD ***
DO 50 I=1, N
X = H2N (I, 65)
IF (SUM2.EQ.X) THEN
END IF
CONTINUE
END IF
*** DETERMINE THE NEW ROW OF H2N ***
IF (FLAG.EQ.1) THEN
DO 60 I=1, N

```

```

ORT 00610
ORT 00620
ORT 00630
ORT 00640
ORT 00650
ORT 00660
ORT 00670
ORT 00680
ORT 00690
ORT 00700
ORT 00710
ORT 00720
ORT 00730
ORT 00740
ORT 00750
ORT 00760
ORT 00770
ORT 00780
ORT 00790
ORT 00800
ORT 00810
ORT 00820
ORT 00830
ORT 00840
ORT 00850
ORT 00860
ORT 00870
ORT 00880
ORT 00890
ORT 00900
ORT 00910
ORT 00920
ORT 00930
ORT 00940
ORT 00950
ORT 00960
ORT 00970
ORT 00980
ORT 00990
ORT 01000
ORT 01010
ORT 01020
ORT 01030
ORT 01040
ORT 01050
ORT 01060
ORT 01070
ORT 01080
ORT 01090
ORT 01100

```

```

60      X=H2N(I,65)
        IF (SUM2.EQ.X) THEN
            ROW=I
            END IF
            CONTINUE
        END IF
        *** DETERMINE THE VALUE OF MT TO BE RETURNED ***
        MT=H2N(ROW,C)
        C=C+1
        RETURN
        END
        C

```

```

ORT01110
ORT01120
ORT01130
ORT01140
ORT01150
ORT01160
ORT01170
ORT01180
ORT01190
ORT01200
ORT01210
ORT01220
ORT01230
ORT01240

```



```

***
C          WILL HAVE THE OPPORTUNITY TO PLOT MORE THAN ONE SECTION'./././
C          OF THE TOTAL RECORD OF '15' POINTS.  ENTER THE NUMBER'./././
C          OF POINTS TO BE PLOTTED.'./././.' :')
      READ (5, *) NI
      IF (NI.LE.IN) THEN
      ELSE
      CALL FRTCMS('CLRSCRN ')
      WRITE(10,30)
      FORMAT('ERROR',/)
      GO TO 19
      END IF
      CALL FRTCMS('CLRSCRN ')
      WRITE(10,40) IN WHICH NUMBER OF THE '15' X,Y PAIRS DO YOU WISH'././
      FORMAT(' AT THE PLOT'./././ YOU SPECIFY TO START THE PLOT MUST BE'
      ' TO START! THE POINT'././ THE ENTIRE RANGE OF POINTS YOU'./
      ' CAUTION! ENOUGH TO ALLOW THE ENTIRE RANGE OF POINTS YOU'./
      ' SMALL ENOUGH TO ALLOW THE ENTIRE RANGE OF POINTS YOU'./
      ' DESIRED TO HAVE PLOTTED AS SPECIFIED BY YOUR PREVIOUS INPUT'
      )
      READ (5, *) R
      IF (R.GT. ((IN+1)-NI)) THEN
      CALL FRTCMS(' CLRSCRN ')
      WRITE(10,50)
      FORMAT('ERROR',/)
      GO TO 39
      END IF
      ND=NI
      RANGE(1) =(ARRAY(R,2) + (ND*INT))
      RANGE(2) =ARRAY(R,2)
      RANGE(3) =1.5D0*MAXY
      RANGE(4) =1.5D0*MINY
      WRITE(10,60)
      FORMAT('1')
      CALL UT PLOT (ARRAY(R,2), ARRAY(R,1), NI, RANGE, 2, 0)
      WRITE(10,70)
      FORMAT(' IF YOU WOULD LIKE ANOTHER PLOT OF THE SAME GRAPH OR'
      ' A PLOT OVER A DIFFERENT RANGE OR FROM ANOTHER STARTING'././
      ' POINT, ENTER A 1.  ENTER ANY OTHER INTEGER TO CONTINUE WITH'
      ' THE PROGRAM.'././.' :')
      READ (5, *) ANS

```

```

PLO00610
PLO00620
PLO00630
PLO00640
PLO00650
PLO00660
PLO00670
PLO00680
PLO00690
PLO00700
PLO00710
PLO00720
PLO00730
PLO00740
PLO00750
PLO00760
PLO00770
PLO00780
PLO00790
PLO00800
PLO00810
PLO00820
PLO00830
PLO00840
PLO00850
PLO00860
PLO00870
PLO00880
PLO00890
PLO00900
PLO00910
PLO00920
PLO00930
PLO00940
PLO00950
PLO00960
PLO00970
PLO00980
PLO00990
PLO01000
PLO01010
PLO01020
PLO01030
PLO01040
PLO01050
PLO01060
PLO01070
PLO01080
PLO01090
PLO01100

```

PL0011110
PL0011120
PL0011130
PL0011140
PL0011150
PL0011160
PL0011170
PL0011180

```
C      IF (ANS - EQ - 1) THEN  
        GO TO 19  
      END IF  
C      END IF  
      RETURN  
      END
```

SUBROUTINE STATS(IN,REP,FLAG)

*** PURPOSE ***

THIS SUBPROGRAM COMPILES THE ACCUMULATED STATISTICS OF THE ELEMENTS OF THE AMPLITUDE SPECTRUM OF THE FFTS.

*** PARAMETER DEFINITIONS ***

IN= INTEGER OF THE NUMBER OF POSITIONS USED IN ARRAY
REP= INTEGER OF THE NUMBER OF THE REPEITION OF THE GENERATION OF THE AMPLITUDE SPECTRUM OF THE FFT
FLAG= AN INTEGER THAT CONTROLS THE POINT OF ENTRANCE OR EXIT FROM THE SUBROUTINE

*** VARIABLE DEFINITIONS ***

IND2P1= POSITIONS USED IN ARRAYS SUMX AND SUMXSQ
ARRAY= AN ARRAY CONTAINING THE VALUES OF THE AMPLITUDE SPECTRUM OF THE FFT
SUMX= AN ARRAY CONTAINING THE SUM OF THE VALUES OF THE AMPLITUDE SPECTRUM OF THE FFT
SUMXSQ= AN ARRAY CONTAINING THE SUM OF THE SQUARES OF THE VALUES OF THE AMPLITUDE SPECTRUM OF THE FFT
SUMX3= AN ARRAY OF THE AMPLITUDE SPECTRUM OF THE SQUARES OF THE VALUES OF THE AMPLITUDE SPECTRUM OF THE FFT
SUMX4= AN ARRAY OF THE AMPLITUDE SPECTRUM OF THE QUARTICS OF THE VALUES OF THE AMPLITUDE SPECTRUM OF THE FFT
XBAR= AN ARRAY OF THE AMPLITUDE SPECTRUM OF THE AVERAGE VALUE OF THE AMPLITUDE SPECTRUM
VAR= AN ARRAY CONTAINING THE VARIANCE OF THE VALUES OF THE AMPLITUDE SPECTRUM
SKEW= THE ELEMENTS OF THE AMPLITUDE SPECTRUM OF THE DISTRIBUTION OF THE ELEMENTS OF THE AMPLITUDE SPECTRUM
KUR= OF THE ELEMENTS OF THE KURTOSIS OF THE DISTRIBUTION OF THE ELEMENTS OF THE AMPLITUDE SPECTRUM
SUMVAR= SUM OF THE VARIANCES OF AN ELEMENT OF THE AMPLITUDE SPECTRUM
AVAR= AVERAGE VARIANCE OF AN ELEMENT OF THE AMPLITUDE SPECTRUM
VARVAR= SPECTRUM OF THE VARIANCES OF AN ELEMENT OF THE AMPLITUDE SPECTRUM
SUMVSQ= VARIANCE OF THE SQUARES OF THE AMPLITUDE SPECTRUM
SUMSKW= AMPLITUDE SPECTRUM OF THE VARIANCES OF AN ELEMENT OF THE AMPLITUDE SPECTRUM
ASKEW= SUM OF THE SKEWNESS OF THE ELEMENTS OF THE AMPLITUDE SPECTRUM
VARSKW= AVERAGE SKEWNESS OF THE ELEMENTS OF THE AMPLITUDE SPECTRUM OF THE SKEWNESS OF THE ELEMENTS OF THE AMPLITUDE SPECTRUM

STA00110
STA00120
STA00130
STA00140
STA00150
STA00160
STA00170
STA00180
STA00190
STA00200
STA00210
STA00220
STA00230
STA00240
STA00250
STA00260
STA00270
STA00280
STA00290
STA00300
STA00310
STA00320
STA00330
STA00340
STA00350
STA00360
STA00370
STA00380
STA00390
STA00400
STA00410
STA00420
STA00430
STA00440
STA00450
STA00460
STA00470
STA00480
STA00490
STA00500
STA00510
STA00520
STA00530
STA00540
STA00550
STA00560
STA00570
STA00580
STA00590
STA00600

CC


```

20 CONTINUE
CC
30 *** COMPUTE THE FINAL STATISTICS IF FLAG EQUALS 1 ***
CC
CC IF (FLAG.EQ. 1) THEN
CC
CC *** COMPUTE STATISTICS ASSOCIATED WITH EACH ELEMENT OF FFT ***
REP=REP-1
REPDP=REP
DO 4 I=1,IND2P1
  XBAR(I)=SUMX(I)/REP
  IF (REP.EQ. 1) THEN
    VAR(I) = ((REPDP*SUMXSQ(I)) - SUMX(I)**2) / REPDP**2
  ELSE
    VAR(I) = ((REPDP*SUMXSQ(I)) - SUMX(I)**2) / (REPDP*(REPDP-1.D0))
  END IF
  SKEW(I) = (SUMX3(I)/REPDP) - (3.D0*(SUMXSQ(I)/REPDP)*
* (SUMX(I)/REPDP) + (2.D0*(SUMX(I)/REPDP)**2)
* (SUMX3(I)/REPDP) - (4.D0*(SUMX(I)/REPDP)**2)
* (SUMX(I)/REPDP) + (6.D0*(SUMX(I)/REPDP)**2**4)
* (SUMXSQ(I)/REPDP) - (3.D0*(SUMX(I)/REPDP)**4)
40 CONTINUE
CC
CC *** OUTPUT SOME DATA ***
50 WRITE(6,50) 2X, N, 11X, MEAN, 17X, VARIANCE, 17X, SKEWNESS,
C FORMAT(1X, I5, 2X, E23.16, 2X, E23.16, 2X, E23.16)
*
60 DO 60 I=1,IND2P1
C WRITE(6,70) I, XBAR(I), VAR(I), SKEW(I), KUR(I)
60 FORMAT(1X, I5, 2X, E23.16, 2X, E23.16, 2X, E23.16)
C CONTINUE
61 WRITE(6,61) 2X, N, 10X, SUM X, 18X, SUM X**2, 16X,
C FORMAT(1X, I5, 2X, E23.16, 2X, E23.16, 2X, E23.16)
*
62 DO 62 I=1,IND2P1
C WRITE(6,63) I, SUMX(I), SUMXSQ(I), SUMX3(I), SUMX4(I)
62 FORMAT(1X, I5, 2X, E23.16, 2X, E23.16, 2X, E23.16)
C CONTINUE
CC
CC *** COMPUTE STATISTICS ASSOCIATED WITH ALL ELEMENTS OF FFT ***
SUMVAR=0.D0
SUMVSO=0.D0
VARVAR=0.D0
SUMSKW=0.D0
STA 011110
STA 011120
STA 011130
STA 011140
STA 011150
STA 011160
STA 011170
STA 011180
STA 011190
STA 011200
STA 011210
STA 011220
STA 011230
STA 011240
STA 011250
STA 011260
STA 011270
STA 011280
STA 011290
STA 011300
STA 011310
STA 011320
STA 011330
STA 011340
STA 011350
STA 011360
STA 011370
STA 011380
STA 011390
STA 011400
STA 011410
STA 011420
STA 011430
STA 011440
STA 011450
STA 011460
STA 011470
STA 011480
STA 011490
STA 011500
STA 011510
STA 011520
STA 011530
STA 011540
STA 011550
STA 011560
STA 011570
STA 011580
STA 011590
STA 011600

```

```

SUMSSQ=0.D0
VARSKW=0.D0
SUMKUR=0.D0
SUMKSKW=0.D0
VARKUR=0.D0
NDP=IND2P1
C
DO 80 I=1,IND2P1
SUMVAR=SUMVAR+VAR(I)
SUMVSO=SUMVSO+(VAR(I)**2)
SUMSKW=SUMSKW+SKW(I)
SUMSSQ=SUMSSQ+(SKW(I)**2)
SUMKUR=SUMKUR+KUR(I)
SUMKSKW=SUMKSKW+(KUR(I)**2)
CONTINUE
80
C
AVAR=SUMVAR/NDP
ASKW=SUMSKW/NDP
AKUR=SUMKUR/NDP
C
DO 90 I=1,IND2P1
VARVAR=VARVAR+(VAR(I)-AVAR)**2
VARSKW=VARSKW+(SKW(I)-ASKW)**2
VARKUR=VARKUR+(KUR(I)-AKUR)**2
CONTINUE
90
C
VARVAR=VARVAR/(NDP-1.D0)
VARSKW=VARSKW/(NDP-1.D0)
VARKUR=VARKUR/(NDP-1.D0)
C
WRITE(6,91) 2X,'SUM OF VARIANCES',7X,'SUM OF VARIANCES**2')
FORMAT(1,'2X','SUM OF VARIANCES',7X,'SUM OF VARIANCES**2')
91
C
WRITE(6,92) SUMVAR,SUMVSO
FORMAT(1X,E23.16,2X,E23.16)
92
C
WRITE(6,93)
FORMAT(6,'0',2X,'SUM OF SKEWNESS',9X,'SUM OF SKEWNESS**2')
93
C
WRITE(6,94) SUMSKW,SUMSSQ
FORMAT(1X,E23.16,2X,E23.16)
94
C
WRITE(6,95)
FORMAT(6,'0',2X,'SUM OF KURTOSIS',9X,'SUM OF KURTOSIS**2')
95
C
WRITE(6,96) SUMKUR,SUMKSKW
FORMAT(1X,E23.16,2X,E23.16)
96
C
WRITE(6,100)
FORMAT(6,'0',3X,'MEAN VARIANCE',7X,'VARIANCE OF THE VARIANCES',
STA 01610
STA 01620
STA 01630
STA 01640
STA 01650
STA 01660
STA 01670
STA 01680
STA 01690
STA 01700
STA 01710
STA 01720
STA 01730
STA 01740
STA 01750
STA 01760
STA 01770
STA 01780
STA 01790
STA 01800
STA 01810
STA 01820
STA 01830
STA 01840
STA 01850
STA 01860
STA 01870
STA 01880
STA 01890
STA 01900
STA 01910
STA 01920
STA 01930
STA 01940
STA 01950
STA 01960
STA 01970
STA 01980
STA 01990
STA 02000
STA 02010
STA 02020
STA 02030
STA 02040
STA 02050
STA 02060
STA 02070
STA 02080
STA 02090
STA 02100

```

```

*
C 101 C WRITE(6,101) A VAR, VAR VAR
C 101 C FORMAT(1X,E23.16,2X,E23.16)
C 102 C WRITE(6,102)
C 102 C FORMAT(10,3X,1 MEAN SKEWNESS,7X,1 VARIANCE OF THE SKEWNESS)
C 103 C WRITE(6,103) ASKEW, VARS KW
C 103 C FORMAT(1X,E23.16,2X,E23.16)
C 104 C WRITE(6,104)
C 104 C FORMAT(10,3X,1 MEAN KURTOSIS,7X,1 VARIANCE OF THE KURTOSIS)
C 105 C WRITE(6,105) AKUR, VARKUR
C 105 C FORMAT(1X,E23.16,2X,E23.16)
C 106 C WRITE(6,106)
C 106 C FORMAT(1)
C
C END IF
C RETURN
C END
STA 02110
STA 02120
STA 02130
STA 02140
STA 02150
STA 02160
STA 02170
STA 02180
STA 02190
STA 02200
STA 02210
STA 02220
STA 02230
STA 02240
STA 02250
STA 02260
STA 02270
STA 02280
STA 02290
STA 02300
STA 02310
STA 02320
STA 02330
STA 02340

```

APPENDIX B

IMSL/NON-IMSL ROUTINES UTILIZED

IMSL ROUTINES

IMSL ROUTINE NAME	-	GGUBFS	GGU00110
COMPUTER	-	IEM/SINGLE	GGU00120
LATEST REVISION	-	JUNE 1, 1980	GGU00130
PURPOSE	-	BASIC UNIFORM (0,1) RANDOM NUMBER GENERATOR - FUNCTION FORM OF GGUBS	GGU00140
USAGE	-	FUNCTION GGUBFS (DSEED)	GGU00150
ARGUMENTS	-	GGUBFS DSEED	GGU00160
	-	RESULTANT DEVIATE. INPUT/OUTPUT DOUBLE PRECISION VARIABLE ASSIGNED AN INTEGER VALUE IN THE EXCLUSIVE RANGE (1.D0, 2147483647.D0). DSEED IS REPLACED BY A NEW VALUE TO BE USED IN A SUBSEQUENT CALL.	GGU00170
PRECISION/HARDWARE	-	SINGLE/ALL	GGU00180
REQD. IMSL ROUTINES	-	NONE REQUIRED	GGU00190
NOTATION	-	INFORMATION ON SPECIAL NOTATION AND CONVENTIONS IS AVAILABLE IN THE MANUAL INTRODUCTION OR THROUGH IMSL ROUTINE UHELP	GGU00200
COPYRIGHT	-	1978 BY IMSL, INC. ALL RIGHTS RESERVED.	GGU00210
WARRANTY	-	IMSL WARRANTS ONLY THAT IMSL TESTING HAS BEEN APPLIED TO THIS CODE. NO OTHER WARRANTY, EXPRESSED OR IMPLIED, IS APPLICABLE.	GGU00220
REAL FUNCTION GGUBFS (DSEED)			GGU00230
DOUBLE PRECISION DSEED			GGU00240
		SPECIFICATIONS FOR ARGUMENTS	GGU00250
		SPECIFICATIONS FOR LOCAL VARIABLES	GGU00260

```

C
C
C
DOUBLE PRECISION  D2P31M, D2P31
DATA              D2P31M = (2**31) - 1
DATA              D2P31 = (2**31) (OR AN ADJUSTED VALUE)
DATA              D2P31M/2147483647.D0/
DATA              D2P31 /2147483648.D0/
DSEED = DMOD(16807.D0*DSEED, D2P31M)
GGUBFS = DSEED / D2P31
RETURN
END
GGU00510
GGU00520
GGU00530
GGU00540
GGU00550
GGU00560
GGU00570
GGU00580
GGU00590
GGU00600

```



```

J = 1
DO 6 I=1,ND2
  X(I) = DCMPLEX(A(J),A(J+1))
  J = J+2
6 CONTINUE
C
GAM = DCMPLEX(ZERO,ZERO)
DO 10 I=1,ND2
  GAM = GAM + X(I)
10 CONTINUE
TP = G(1)-G(2)
GAM = DCMPLEX(TP,ZERO)
C
MTWO = 2
M = 1
DO 15 I=1,IMAX
  IF (ND2.LE.MTWO) GO TO 20
  MTWO = MTWO+MTWO
  M = M+1
15 CONTINUE
20 IF (ND2.EQ.MTWO) GO TO 25
C
25 CALL FFT2C(X,M,IWK)
30 ALPH = X(1) + B(2)
  X(1) = B(1) + X(1)
  ND4 = (ND2+1)/2
  IF (ND4.LT.2) GO TO 40
  NP2 = ND2 + 2
  THETA = RPI/ND2
  TP = THETA
  XIMAG = DCMPLEX(ZERO,ONE)
C
DO 35 K = 2,ND4
  NMK = NP2 - K
  S1 = DCONJG(X(NMK))
  ALPH = X(K) + S1
  BETA = XIMAG*(S1-X(K))
  S1 = DCMPLEX(DCOS(THETA),DSIN(THETA))
  X(K) = (ALPH+BETA*S1)*HALF
  X(NMK) = DCONJG(ALPH-BETA*S1)*HALF
  THETA = THETA + TP
35 CONTINUE
40 X(ND2P1) = GAM
  ND2=N/2
  DO 90 I=2,ND2

```

```

FFT01180
FFT01190
FFT01200
FFT01210
FFT01220
FFT01230
FFT01240
FFT01250
FFT01260
FFT01270
FFT01280
FFT01290
FFT01300
FFT01310
FFT01320
FFT01330
FFT01340
FFT01350
FFT01360
FFT01370
FFT01380
FFT01390
FFT01400
FFT01410
FFT01420
FFT01430
FFT01440
FFT01450
FFT01460
FFT01470
FFT01480
FFT01490
FFT01500
FFT01510
FFT01520
FFT01530
FFT01540
FFT01550
FFT01560
FFT01570
FFT01580
FFT01590
FFT01600
FFT01610
FFT01620
FFT01630
FFT01640
FFT01650
FFT01660
FFT01670

```

COMPUTE THE CENTER COEFFICIENT

DETERMINE THE SMALLEST M SUCH THAT N IS LESS THAN OR EQUAL TO 2**M

N IS NOT A POWER OF TWO, CALL FFTCC
N IS A POWER OF TWO, CALL FFT2C

DECOMPOSE THE COMPLEX VECTOR X INTO THE COMPONENTS OF THE TRANSFORM OF THE INPUT DATA.


```
C 90      X (N+2-I) = DCONJG (X (I) )  
C 9005   CONTINUE  
          RETURN  
          END
```

```
FFT01680  
FFT01690  
FFT01700  
FFT01710
```



```

DO 10 I=1,N CONJG (A(I))
A(I) = CONJG (A(I))
10 CONTINUE
CALL FFT2C (A, M, IWK)
DO 20 I=1,N
A(I) = CONJG(A(I))/N
20 CONTINUE

```

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```

SUBROUTINE FFT2C (A, M, IWK)
M, IWK(1)
A(1)
1 ISP, J, JJ, N2, LM, NN, JK
N4, N8, C1, C2, B3, TWOPI, TEMP
BO, B1, B2, Z0(2), Z1(2), Z2(2), Z3(2)
ZERO, ZA1, ZA2, ZA3, AK2
ZA0, Z0(1), Z1(1), Z2(1), Z3(1)
(ZA3, Z3(1)), (A0, Z0(1)), (A1, Z1(1))
(B1, Z1(2)), (A2, Z2(1)), (B2, Z2(2)), (A3, Z3(1))
(B3, Z3(2))
SQ = 7071067811865475D0/
SK = 3826834323650898D0/
CK = 9238795325112868D0/
TWOPI/6.283185307179586D0/
ZERO/0.0D0/ ONE/1.0D0/
SQ = SQRT2/2, SK = SIN (PI/8), CK = COS (PI/8)
TWOPI = 2*PI
FIRST EXECUTABLE STATEMENT

```

```

MP = M+1
N = 2**M
IWK(1) = 1
MM = (M/2)*2
KN = N+1
DO 5 I=2,MP
IWK(I) = IWK(I-1) + IWK(I-1)
5 CONTINUE
RAD = TWOPI/N
MK = M - 4

```

INITIALIZE WORK VECTOR

FFTT00610
FFTT00620
FFTT00630
FFTT00640
FFTT00650
FFTT00660
FFTT00670
FFTT00680
FFTT00690
FFTT00700
FFTT00710
FFTT00720
FFTT00730
FFTT00740
FFTT00750
FFTT00760
FFTT00770
FFTT00780
FFTT00790
FFTT00800
FFTT00810
FFTT00820
FFTT00830
FFTT00840
FFTT00850
FFTT00860
FFTT00870
FFTT00880
FFTT00890
FFTT00900
FFTT00910
FFTT00920
FFTT00930
FFTT00940
FFTT00950
FFTT00960
FFTT00970
FFTT00980
FFTT00990
FFTT01000
FFTT01010
FFTT01020
FFTT01030
FFTT01040
FFTT01050
FFTT01060
FFTT01070
FFTT01080
FFTT01090
FFTT01100

```

FFTT01110
FFTT011120
FFTT011130
FFTT011140
FFTT011150
FFTT011160
FFTT011170
FFTT011180
FFTT011190
FFTT011200
FFTT011210
FFTT011220
FFTT011230
FFTT011240
FFTT011250
FFTT011260
FFTT011270
FFTT011280
FFTT011290
FFTT011300
FFTT011310
FFTT011320
FFTT011330
FFTT011340
FFTT011350
FFTT011360
FFTT011370
FFTT011380
FFTT011390
FFTT011400
FFTT011410
FFTT011420
FFTT011430
FFTT011440
FFTT011450
FFTT011460
FFTT011470
FFTT011480
FFTT011490
FFTT011500
FFTT011510
FFTT011520
FFTT011530
FFTT011540
FFTT011550
FFTT011560
FFTT011570
FFTT011580
FFTT011590
FFTT011600

```

```

1  KB = (MM . EQ. M) GO TO 15
2  IF (KN . EQ. 1) GO TO 15
3  K0 = IWK (MM+1) + KB
4  K2 = K2 - 1
5  K0 = K0 - 1
6  AK2 = A (K2)
7  A (K2) = A (K0) - AK2
8  A (K0) = A (K0) + AK2
9  IF (K0 . EQ. 1) GO TO 10
10 S1 = ONE
11 JJ = ZERO
12 K = MM - 1
13 J = 4
14 IF (K . GE. 1) GO TO 30
15 GO TO 70
16 IF (IWK (J) . GT. JJ) GO TO 25
17 JJ = JJ - IWK (J)
18 J = J - 1
19 IF (IWK (J) . GT. JJ) GO TO 25
20 JJ = JJ - IWK (J)
21 J = J - 1
22 K = K + 2
23 GO TO 20
24 JJ = IWK (J) + JJ
25 ISP = IWK (K)
26 IF (JJ . EQ. 0) GO TO 40
27 C2 = JJ * ISP * RAD
28 C1 = DCOS (C2)
29 S1 = DSIN (C2)
30 C2 = C1 * (S1 - S1 * S1)
31 S2 = C1 * (S1 + S1)
32 C3 = C2 * (S1 - S2 * S1)
33 S3 = C2 * (S1 + S2 * S1)
34 JSP = ISP + KB
35 DO I=1,ISP - I
36 K1 = K0 + ISP
37 K2 = K1 + ISP
38 K3 = K2 + ISP
39 ZA0 = A (K0)
40 ZA1 = A (K1)
41 ZA2 = A (K2)
42 ZA3 = A (K3)
43 IF (S1 . EQ. ZERO) GO TO 45

```

RESET TRIGONOMETRIC PARAMETERS

DETERMINE FOURIER COEFFICIENTS
IN GROUPS OF 4

```

TEMP = A1 * S1 - B1 * S1 * C1
A1 = TEMP
B1 = A2 * S2 - B2 * S2 * C2
TEMP = A3 * S3 - B3 * S3 * C3
A2 = TEMP
B2 = A0 - A2
TEMP = A1 - A3
A3 = TEMP
B0 = B0 - B2
TEMP = B1 - B3
B1 = TEMP
B3 = DCMPPLX (A0+A1, B0+B1)
A (K1) = DCMPPLX (A0-A1, B0-B1)
A (K2) = DCMPPLX (A2-E3, B2+A3)
A (K3) = DCMPPLX (A2+B3, B2-A3)
50 CONTINUE
IF (K .LE. 1) GO TO 55
K = K - 2
GO TO 30
55 KB = K3 + ISF

```

45

C
C
CHECK FOR COMPLETION OF FINAL
ITERATION

```

IF (KN .LE. KB) GO TO 70
IF (J .NE. 1) GO TO 60
K = MK
J = J - 1
GO TO 20
C2 = C1
IF (J .NE. 2) GO TO 65
C1 = C1 * CK + S1 * SK
S1 = S1 * CK - C2 * SK
GO TO 35
C1 = (C1 - S1) * SQ
S1 = (C2 + S1) * SQ
GO TO 35
70 CONTINUE

```

C
C
C
PERMUTE THE COMPLEX VECTOR IN
REVERSE BINARY ORDER TO NORMAL
ORDER

FFT 01610
FFT 01620
FFT 01630
FFT 01640
FFT 01650
FFT 01660
FFT 01670
FFT 01680
FFT 01690
FFT 01700
FFT 01710
FFT 01720
FFT 01730
FFT 01740
FFT 01750
FFT 01760
FFT 01770
FFT 01780
FFT 01790
FFT 01800
FFT 01810
FFT 01820
FFT 01830
FFT 01840
FFT 01850
FFT 01860
FFT 01870
FFT 01880
FFT 01890
FFT 01900
FFT 01910
FFT 01920
FFT 01930
FFT 01940
FFT 01950
FFT 01960
FFT 01970
FFT 01980
FFT 01990
FFT 02000
FFT 02010
FFT 02020
FFT 02030
FFT 02040
FFT 02050
FFT 02060
FFT 02070
FFT 02080
FFT 02090
FFT 02100

FFT02110
 FFT02120
 FFT02130
 FFT02140
 FFT02150
 FFT02160
 FFT02170
 FFT02180
 FFT02190
 FFT02200
 FFT02210
 FFT02220
 FFT02230
 FFT02240
 FFT02250
 FFT02260
 FFT02270
 FFT02280
 FFT02290
 FFT02300
 FFT02310
 FFT02320
 FFT02330
 FFT02340
 FFT02350
 FFT02360
 FFT02370
 FFT02380
 FFT02390
 FFT02400
 FFT02410
 FFT02420
 FFT02430
 FFT02440
 FFT02450
 FFT02460
 FFT02470
 FFT02480
 FFT02490
 FFT02500
 FFT02510
 FFT02520
 FFT02530
 FFT02540
 FFT02550
 FFT02560
 FFT02570
 FFT02580
 FFT02590
 FFT02600

INITIALIZE WORK VECTOR

```

C
IF (M .LE. 1) GO TO 9005
MP = M+1
JJ = 1
IWK(1) = 1
DO 75 I = 2, MP
  IWK(I) = IWK(I-1) * 2
75 CONTINUE
N4 = IWK(MP-2)
IF (M .GT. 2) N8 = IWK(MP-3)
N2 = IWK(MP-1)
LN = N2
LN = IWK(MP) + 1
MP = MP-4
C
J = 2
JK = JJ + N2
AK2 = A(J)
A(J) = A(JK)
A(JK) = AK2
J = J+1
IF (JJ .GT. N4) GO TO 85
JJ = JJ + N4
GO TO 105
85 JJ = JJ - N4
IF (JJ .GT. N8) GO TO 90
JJ = JJ + N8
GO TO 105
90 JJ = JJ - N8
K = MP
95 IF (IWK(K) .GE. JJ) GO TO 100
JJ = JJ - IWK(K)
K = K - 1
GO TO 95
100 JJ = IWK(K) + JJ
105 IF (JJ .LE. J) GO TO 110
K = NN - J
JK = NN - JJ
AK2 = A(J)
A(J) = A(JJ)
A(JJ) = AK2
AK2 = A(K)
A(K) = A(JK)
A(JK) = AK2
J = J + 1
110
  
```

DETERMINE INDICES AND SWITCH A

CYCLE REPEATED UNTIL LIMITING NUMBER OF CHANGES IS ACHIEVED

```

C
IF (J .LE. LM) GO TO 80
C
9005 RETURN
  
```

END

FFT02610

NON-IMSL ROUTINE

```

.....
SUBROUTINE UTPLOT
PURPOSE
    PRINTS GRAPHS ON THE STANDARD OUTPUT PRINTER
FEATURES
1) FULL CONTROL OVER SCALING
2) ABILITY TO PLOT SINGLE OR DOUBLE PRECISION VECTORS
CALLING SEQUENCE
CALL UTPLOT (X,Y,N,RANGE,K,MODCUR)
DESCRIPTION OF ARGUMENTS
X      VECTOR OF ABSCISSAE
Y      VECTOR OF ASSOCIATED ORDINATES
N      NUMBER OF (X,Y) PAIRS
RANGE  4 WORD SCALING VECTOR WHERE
        RANGE (1) = MAXIMUM X TO BE PLOTTED
        RANGE (2) = MINIMUM X TO BE PLOTTED
        RANGE (3) = MAXIMUM Y TO BE PLOTTED
        RANGE (4) = MINIMUM Y TO BE PLOTTED
K      EVERY KTH ELEMENT OF X & Y WILL BE PLOTTED, E.G.,
        FOR REAL*4 DATA (SINGLE PRECISION) K=1
        FOR REAL*8 DATA (DOUBLE PRECISION) K=2.
MODCUR CONTROLS THE NUMBER OF CURVES ON ONE GRAPH
=0 THERE IS ONLY 1 CURVE ON THIS GRAPH
=1 THIS IS THE FIRST OF TWO OR MORE CURVES ON THIS GRAPH
=2 THIS IS AN INTERMEDIATE CURVE ON THIS GRAPH
=3 THIS IS THE LAST CURVE ON THIS GRAPH
SCALING
    SCALING IS PERFORMED ONLY ON THE FIRST SET OF POINTS (WHEN
.....
UTP00110
UTP00120
UTP00130
UTP00140
UTP00150
UTP00160
UTP00170
UTP00180
UTP00190
UTP00200
UTP00210
UTP00220
UTP00230
UTP00240
UTP00250
UTP00260
UTP00270
UTP00280
UTP00290
UTP00300
UTP00310
UTP00320
UTP00330
UTP00340
UTP00350
UTP00360
UTP00370
UTP00380
UTP00390
UTP00400
UTP00410
UTP00420
UTP00430
UTP00440
UTP00450
UTP00460
UTP00470
UTP00480
UTP00490
UTP00500
UTP00510
UTP00520
UTP00530
UTP00540
UTP00550
UTP00560
UTP00570

```



```

IF(YMIN.EQ.0.) GO TO 889
YMIN=0.
YRANGE=YMAX
GO TO 299
298 IF (XRANGE.NE.0.) GO TO 299
IF(XMIN.EQ.0.) GO TO 887
XMIN=0.
XRANGE=XMAX
C
C
C BLANKING OUT MATRIX-(GRID)
DO 300 I=1,61
DO 301 JJ=1,81
GRID(I,JJ)=BLANK
301 CONTINUE
300 IF(XMAX*XMIN.GE.0.) GO TO 222
IYAXIS=80.*(-XMIN)/XRANGE+1.5
DO 40 I=1,61
40 GRID(I,IYAXIS)=DOT
222 IF(YMAX*YMIN.GE.0.) GO TO 333
IXAXIS=60.*YMAX/YRANGE+1.5
DO 60 I=1,81
60 GRID(IXAXIS,I)=DOT
C
C
C COMPUTE PROPER SCALE NUMBERS
333 XINCR=XRANGE/4.
YINCR=YRANGE/6.
XSCALE(1)=XMAX
XSCALE(5)=XMIN
DO 80 I=2,4
80 XSCALE(I)=XSCALE(I-1)-XINCR
IF(ABS(XSCALE(I)).LT.1.E-4) XSCALE(I)=0.
CONTINUE
YSCALE(1)=YMAX
YSCALE(7)=YMIN
DO 81 I=2,6
81 YSCALE(I)=YSCALE(I-1)-YINCR
IF(ABS(YSCALE(I)).LT.1.E-4) YSCALE(I)=0.
CONTINUE
DO 85 II=1,2
85 JJ=6-II
XT=XSCALE(JJ)
XSCALE(JJ)=XSCALE(II)
XSCALE(II)=XT
C
C
C PLACING POINTS IN THEIR PROPER GRID POSITIONS
444 IF(MODCUR.LT.2) JSET=0

```

```

UTP 01580
UTP 01590
UTP 01600
UTP 01610
UTP 01620
UTP 01630
UTP 01640
UTP 01650
UTP 01660
UTP 01670
UTP 01680
UTP 01690
UTP 01700
UTP 01710
UTP 01720
UTP 01730
UTP 01740
UTP 01750
UTP 01760
UTP 01770
UTP 01780
UTP 01790
UTP 01800
UTP 01810
UTP 01820
UTP 01830
UTP 01840
UTP 01850
UTP 01860
UTP 01870
UTP 01880
UTP 01890
UTP 01900
UTP 01910
UTP 01920
UTP 01930
UTP 01940
UTP 01950
UTP 01960
UTP 01970
UTP 01980
UTP 01990
UTP 02000
UTP 02010
UTP 02020
UTP 02030
UTP 02040
UTP 02050
UTP 02060
UTP 02070

```

```

UTP02080
UTP02090
UTP02100
UTP02110
UTP02120
UTP02130
UTP02140
UTP02150
UTP02160
UTP02170
UTP02180
UTP02190
UTP02200
UTP02210
UTP02220
UTP02230
UTP02240
UTP02250
UTP02260
UTP02270
UTP02280
UTP02290
UTP02300
UTP02310
UTP02320
UTP02330
UTP02340
UTP02350
UTP02360
UTP02370
UTP02380
UTP02390
UTP02400
UTP02410
UTP02420
UTP02430
UTP02440
UTP02450
UTP02460
UTP02470
UTP02480
UTP02490
UTP02500
UTP02510
UTP02520
UTP02530
UTP02540
UTP02550
UTP02560
UTP02570

IF(JERR.GT.0) GO TO 885
JSET=JSET+1
IF(JSET.GT.4) JSET=1
DO 700 I=1, KLATA, KKZ /YRANGE+1.5
IPTX=60.*(X(I)-XMIN)/XSCALE
IF(IPTX.GT.81) GO TO 70
IF(IPTX.LE.0) OR IPTX.IE.0) GO TO 70
GRID(IPTX, IPTY) = XCHAR(JSET)
GO TO 700
IERR=IERR+1
CONTINUE
OUTPUT SECTION WITH GRAPH
C
C
IF(MODCUR.EQ.1) OR MODCUR.EQ.2) RETURN
AXR=ABS(XRANGE)
AYR=ABS(YRANGE)
IF(AXR.LT.1.E+8) AND AYR.GE..95) GO TO 400
WRITE(6,17) XSCALE
FORMAT(12X,1PE10.3,4(10X,E10.3)/15X,***,8('+*****'),'+***)
17 GO TO 401
WRITE(6,117) XSCALE
FORMAT(9X,F11.2,4(9X,F11.2)/15X,***,8('+*****'),'+***)
117
118
401 II=1
DO 101 IK=1,61
IF(MOD(IK-1,10).NE.0) GO TO 92
IF(AYR.LT.1.E+8) AND AYR.GE..95) GO TO 404
WRITE(6,18) YSCALE(II), GRID(IK,IX), IX=1,81, YSCALE(II)
FORMAT(3X,1PE10.3,2X,1H+,1X,81A1,1X,1H+,2X,E10.3)
18 GO TO 405
WRITE(6,118) YSCALE(II), GRID(IK,IX), IX=1,81, YSCALE(II)
FORMAT(2X,F11.2,1X,81A1,1X,1H+,2X,E10.3)
118
405 II=II+1
GO TO 101
WRITE(6,19) (GRID(IK,IX), IX=1,81)
FORMAT(15X,*,8A1,*)
19 CONTINUE
IF(AXR.LT.1.E+8) AND AYR.GE..95) GO TO 402
WRITE(6,22) XSCALE
FORMAT(15X,***,8('+*****'),'+***/12X,1PE10.3,4(10X,E10.3),//)
22 GO TO 403
WRITE(6,217) XSCALE
FORMAT(15X,***,8('+*****'),'+***/8X,F11.2,4(9X,F11.2),//)
217
218
403 IF(IERR.GT.0) WRITE(6,20) IERR
FORMAT(10X,NUMBER OF POINTS OUT OF RANGE =', I4)
20 RETURN
1000
C
889 WRITE(6,888)
888 FORMAT(' ALL Y VALUES=0. CANNOT SETUP PLOT GRID. CHECK MAX & MIN Y
1 WHEN MODCUR=0 OR 1.')

```

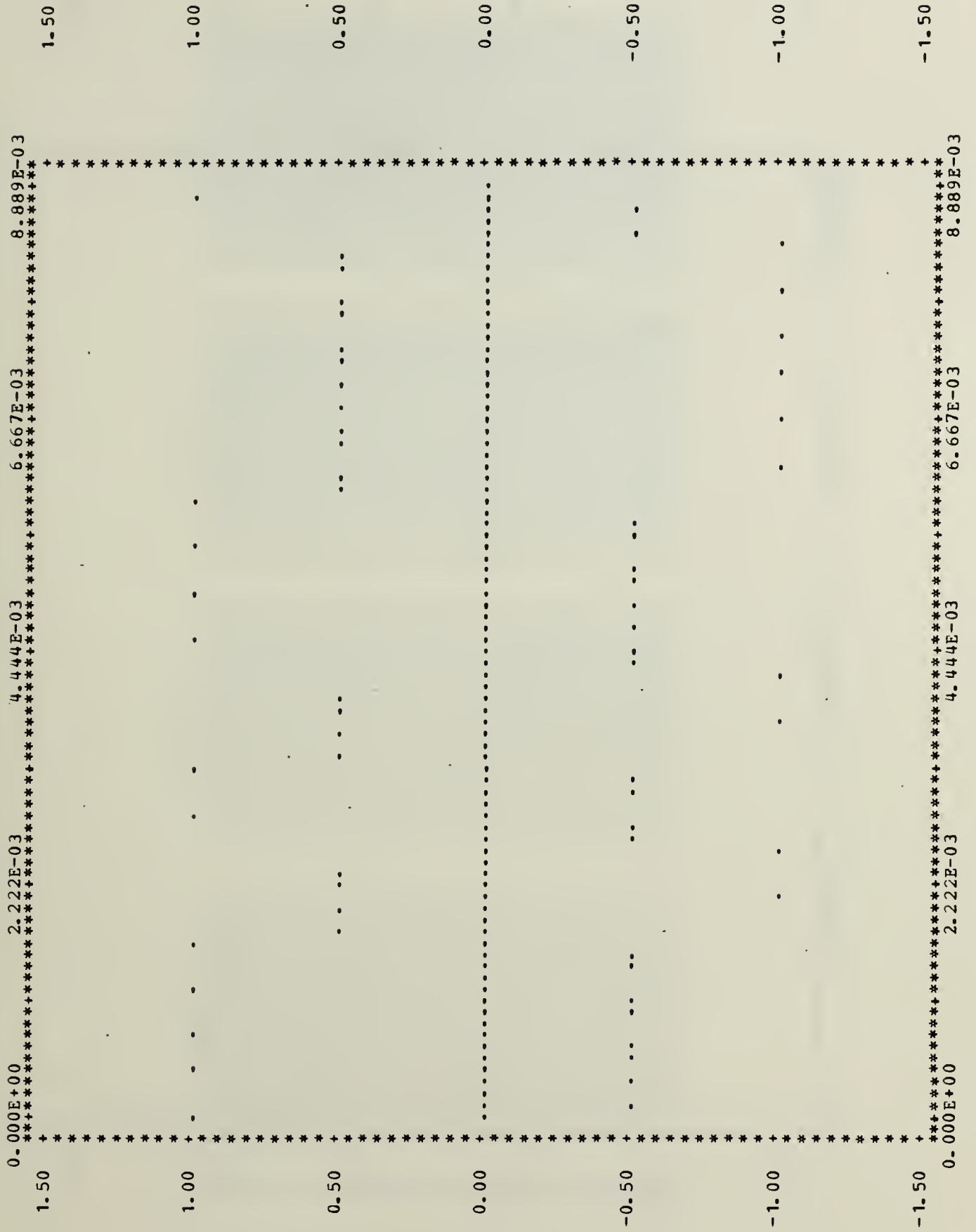
```

JERR=10
RETURN
887 WRITE(6, 886)
886 FORMAT(' ALL X VALUES=0.. CANNOT SETUP PLOT GRID. CHECK MAX & MIN
1 WHEN MODCUR=0 OR 1..')
JERR=10
RETURN
885 WRITE(6, 884)
884 FORMAT(' GRID NOT SETUP WHEN MODCUR LAST 0 OR 1. NO PLOT UNTIL GRID
1D PROPERLY SETUP.')
RETURN
END
UTP02580
UTP02590
UTP02600
UTP02610
UTP02620
UTP02630
UTP02640
UTP02650
UTP02660
UTP02670
UTP02680
UTP02690

```

APPENDIX C
 REPRESENTATIVE RESULTS OF TRIAL SIMULATIONS

MODULATION TECHNIQUE = BPSK
 BIFOLAR LOGIC
 BAUD OR SYMBOL RATE = 1200 HZ
 BITS PER BINARY CODE WORD = 1
 BIT RATE = 0.1200000000000000E+04
 CARRIER FREQUENCY = 2400 HZ
 MAXIMUM CARRIER AMPLITUDE = 1 VOLT(S)
 INITIAL PHASE ANGLE = 0 DEGREES
 TIME BETWEEN SAMPLES = 0.1388888888888889E-03 SEC
 NUMBER OF SAMPLES GENERATED = 64
 SEED FOR RANDOM NUMBER GENERATOR = 1
 NUMBER OF TIMES SIMULATION REPEATS = 100
 SUM OF VARIANCES SUM OF VARIANCES**2
 0.2015734723265312E+03 0.2783281622639908E+04
 SUM OF SKEWNESS SUM OF SKEWNESS**2
 -0.1039295264723739E+05 0.1054665065832765E+08
 SUM OF KURTOSIS SUM OF KURTOSIS**2
 0.7097901826525830E+04 0.5645466161770898E+07
 MEAN VARIANCE VARIANCE OF THE VARIANCES
 0.6108287040197914E+01 0.4850040606187702E+02
 MEAN SKEWNESS VARIANCE OF THE SKEWNESS
 -0.3149379590071935E+03 0.2272973551108844E+06
 MEAN KURTOSIS VARIANCE OF THE KURTOSIS
 0.2150879341371464E+03 0.1287122850373493E+06





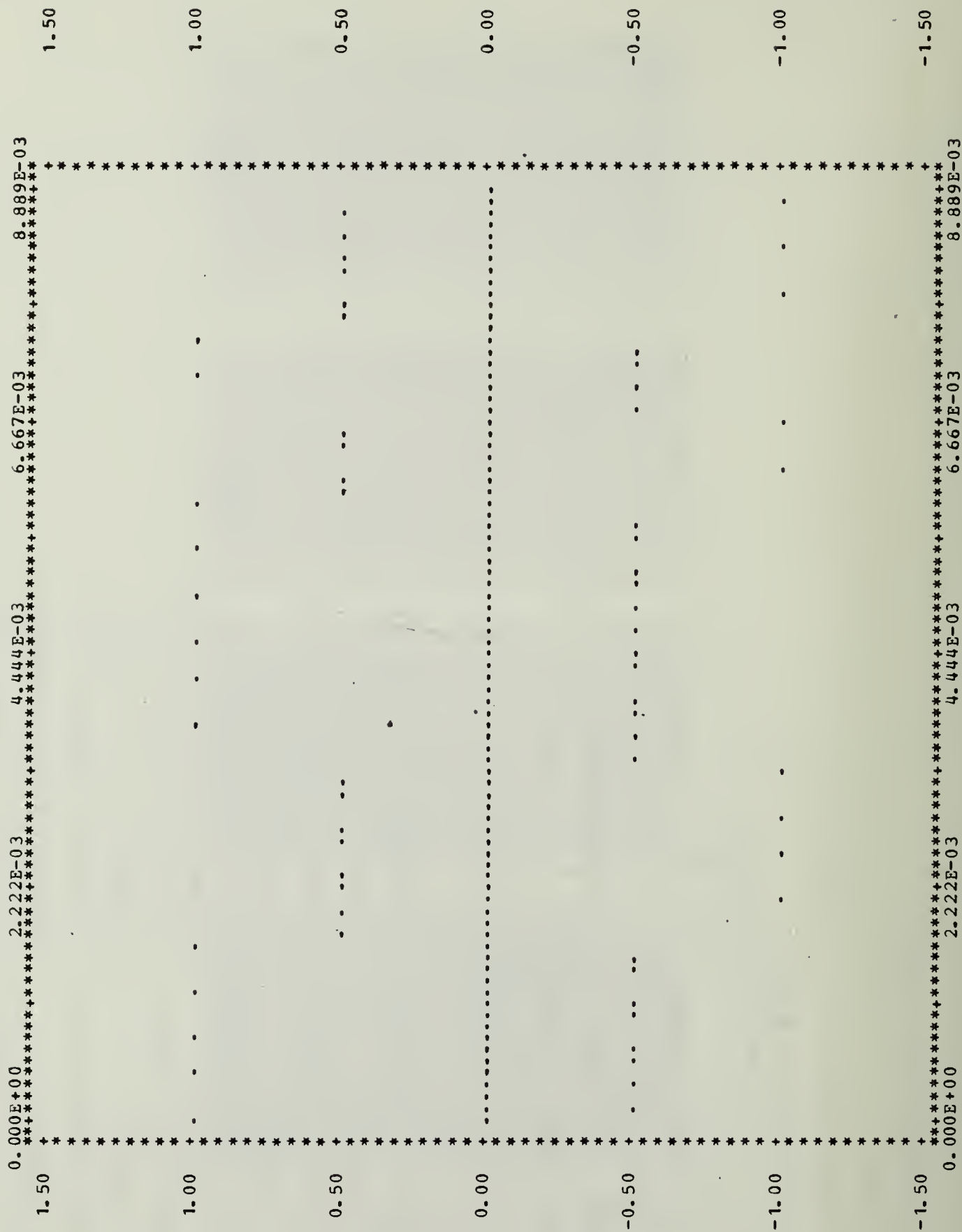
N	MEAN	STDEV	VARIANCE	SKEWNESS	KURTOSIS
1	1000	000000	1561758	1465494	222044
2	1047	093608	2709840	486164	185959
3	1781	990141	605257	137741	940280
4	2374	133369	1061217	159158	255598
5	2634	626472	1327139	386360	465981
6	2930	178593	1802009	105244	104337
7	2742	584859	1750464	180766	923033
8	2852	400569	1444992	256107	540708
9	2056	852875	1931984	334168	840463
10	1456	809184	949876	291054	219377
11	1420	945625	1408870	169178	200110
12	3224	566286	892728	275337	507957
13	4083	755764	1296676	472269	348172
14	5177	315729	992769	894275	234817
15	7437	747541	1296676	609306	238158
16	9168	103367	1066781	295108	465502
17	8770	044710	2027197	672707	937744
18	9524	106864	1961533	346454	992129
19	8962	219620	1842175	475918	137869
20	7991	136976	1591304	787280	764076
21	8132	813049	1673585	978728	583174
22	6361	858526	856676	186177	613687
23	5294	298817	700619	225233	190378
24	4057	930055	493094	560051	139019
25	3416	828808	2501314	199993	678188
26	2867	533342	1412648	333481	172664
27	2020	303908	1060744	509054	415066
28	1365	571743	4519751	376518	261453
29	1080	000000	1003636	336363	470443
30	1080	000000	1003636	336363	470443
31	1080	000000	1003636	336363	470443
32	1080	000000	1003636	336363	470443
33	1080	000000	1003636	336363	470443

N	X	X*	X**2	X**3	X**4
1	1000	0000	0000	0000	0000
2	1047	4936	0873	8495	3879
3	1781	9901	4950	2563	8799
4	2374	1333	1942	2217	9504
5	2634	1586	4920	7520	1305
6	2930	1785	3409	9705	1808
7	2742	1588	5997	4633	1305
8	2852	4055	5526	2039	1305
9	2056	8528	7546	7849	1305
10	1456	8091	8409	3505	1305
11	1456	8889	2005	7782	1305
12	1920	9456	2582	2921	1305
13	3224	5552	8632	3947	1305
14	4083	7557	6208	7475	1305
15	5391	8779	5905	8215	1305
16	5177	3157	2418	3053	1305
17	7437	7475	4183	0537	1305
18	8281	1071	4775	3164	1305
19	9168	0336	7747	2456	1305
20	8770	0447	1083	3351	1305
21	9524	1068	6459	5133	1305
22	8962	2196	2094	1566	1305
23	7911	1330	4990	1235	1305
24	8132	1858	2686	7442	1305
25	6294	2930	5588	1764	1305
26	4057	9300	5588	5899	1305
27	3416	8288	8088	0886	1305
28	2867	5339	0883	1556	1305
29	2020	3037	9083	7567	1305
30	1365	5717	4000	7546	1305
31	1080	0000	0000	0075	1305
32	1080	0000	0000	0075	1305
33	1080	0000	0000	0075	1305
34	1080	0000	0000	0075	1305
35	1080	0000	0000	0075	1305
36	1080	0000	0000	0075	1305
37	1080	0000	0000	0075	1305
38	1080	0000	0000	0075	1305
39	1080	0000	0000	0075	1305
40	1080	0000	0000	0075	1305
41	1080	0000	0000	0075	1305
42	1080	0000	0000	0075	1305
43	1080	0000	0000	0075	1305
44	1080	0000	0000	0075	1305
45	1080	0000	0000	0075	1305
46	1080	0000	0000	0075	1305
47	1080	0000	0000	0075	1305
48	1080	0000	0000	0075	1305
49	1080	0000	0000	0075	1305
50	1080	0000	0000	0075	1305
51	1080	0000	0000	0075	1305
52	1080	0000	0000	0075	1305
53	1080	0000	0000	0075	1305
54	1080	0000	0000	0075	1305
55	1080	0000	0000	0075	1305
56	1080	0000	0000	0075	1305
57	1080	0000	0000	0075	1305
58	1080	0000	0000	0075	1305
59	1080	0000	0000	0075	1305
60	1080	0000	0000	0075	1305
61	1080	0000	0000	0075	1305
62	1080	0000	0000	0075	1305
63	1080	0000	0000	0075	1305
64	1080	0000	0000	0075	1305
65	1080	0000	0000	0075	1305
66	1080	0000	0000	0075	1305
67	1080	0000	0000	0075	1305
68	1080	0000	0000	0075	1305
69	1080	0000	0000	0075	1305
70	1080	0000	0000	0075	1305
71	1080	0000	0000	0075	1305
72	1080	0000	0000	0075	1305
73	1080	0000	0000	0075	1305
74	1080	0000	0000	0075	1305
75	1080	0000	0000	0075	1305
76	1080	0000	0000	0075	1305
77	1080	0000	0000	0075	1305
78	1080	0000	0000	0075	1305
79	1080	0000	0000	0075	1305
80	1080	0000	0000	0075	1305
81	1080	0000	0000	0075	1305
82	1080	0000	0000	0075	1305
83	1080	0000	0000	0075	1305
84	1080	0000	0000	0075	1305
85	1080	0000	0000	0075	1305
86	1080	0000	0000	0075	1305
87	1080	0000	0000	0075	1305
88	1080	0000	0000	0075	1305
89	1080	0000	0000	0075	1305
90	1080	0000	0000	0075	1305
91	1080	0000	0000	0075	1305
92	1080	0000	0000	0075	1305
93	1080	0000	0000	0075	1305
94	1080	0000	0000	0075	1305
95	1080	0000	0000	0075	1305
96	1080	0000	0000	0075	1305
97	1080	0000	0000	0075	1305
98	1080	0000	0000	0075	1305
99	1080	0000	0000	0075	1305
100	1080	0000	0000	0075	1305

```

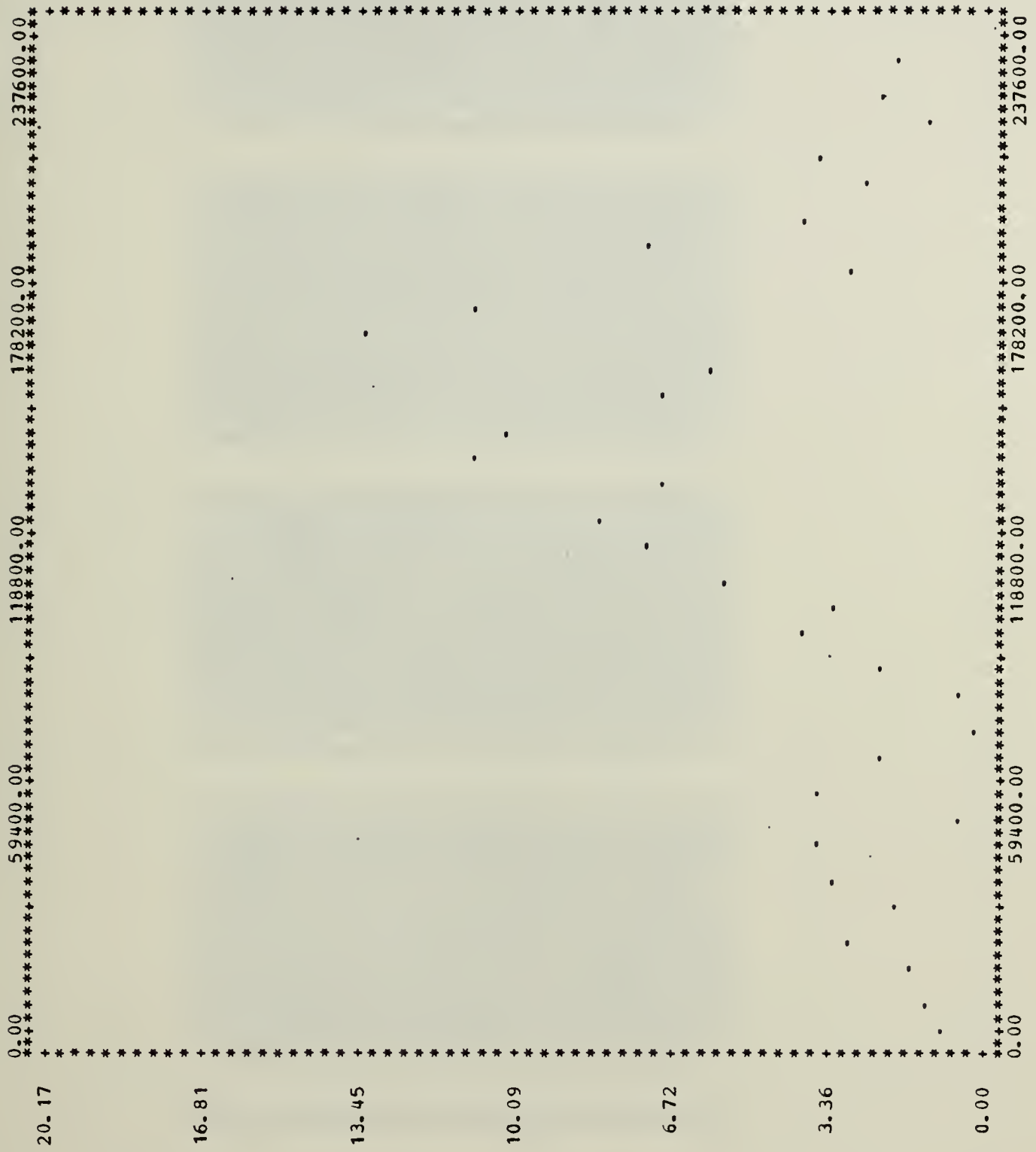
MODULATION TECHNIQUE = DBPSK
BIFOIAR LOGIC
BAUD OR SYMBOL RATE = 1200 HZ
BITS PER BINARY CODE WORD = 1
BIT RATE = 0.1200000000000000E+04
CARRIER FREQUENCY = 2400 HZ
MAXIMUM CARRIER AMPLITUDE = 1 VOLT(S)
INITIAL PHASE ANGLE = 0 DEGREES
TIME BETWEEN SAMPLES = 0.1388888888888889E-03 SEC
NUMBER OF SAMPLES GENERATED = 64
SEED FOR RANDOM NUMBER GENERATOR = 1
NUMBER OF TIMES SIMULATION REPEATS = 100
SUM OF VARIANCES SUM OF VARIANCES**2
0.2149282745632018E+03 0.3048987837599078E+04
SUM OF SKEWNESS SUM OF SKEWNESS**2
-0.9719603900974997E+04 0.8598103883304453E+07
SUM OF KURTOSIS SUM OF KURTOSIS**2
0.8665643426712656E+04 0.8293411900734219E+07
MEAN VARIANCE VARIANCE OF THE VARIANCES
0.6512978017066721E+01 0.5153639719133948E+02
MEAN SKEWNESS VARIANCE OF THE SKEWNESS
-0.2945334515446968E+03 0.1792298562094682E+06
MEAN KURTOSIS VARIANCE OF THE KURTOSIS
0.2625952553549290E+03 0.1880579703838077E+06

```



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MODULATION TECHNIQUE = ORTHOGONAL BPSK
BIFOLAR LOGIC

BAUD OR SYMBOL RATE = 1200 HZ

BITS PER BINARY CODE WORD = 3

BIT RATE = 0.9600000000000000E+04

CARRIER FREQUENCY = 19200 HZ

MAXIMUM CARRIER AMPLITUDE = 1 VOLT(S)

INITIAL PHASE ANGLE = 0 DEGREES

TIME BETWEEN SAMPLES = 0.2450980392156863E-04 SEC

NUMBER OF SAMPLES GENERATED = 64

SEED FOR RANDOM NUMBER GENERATOR = 1

NUMBER OF TIMES SIMULATION REPEATS = 100

SUM OF VARIANCES SUM OF VARIANCES**2

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SUM OF SKEWNESS SUM OF SKEWNESS**2

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SUM OF KURTOSIS SUM OF KURTOSIS**2

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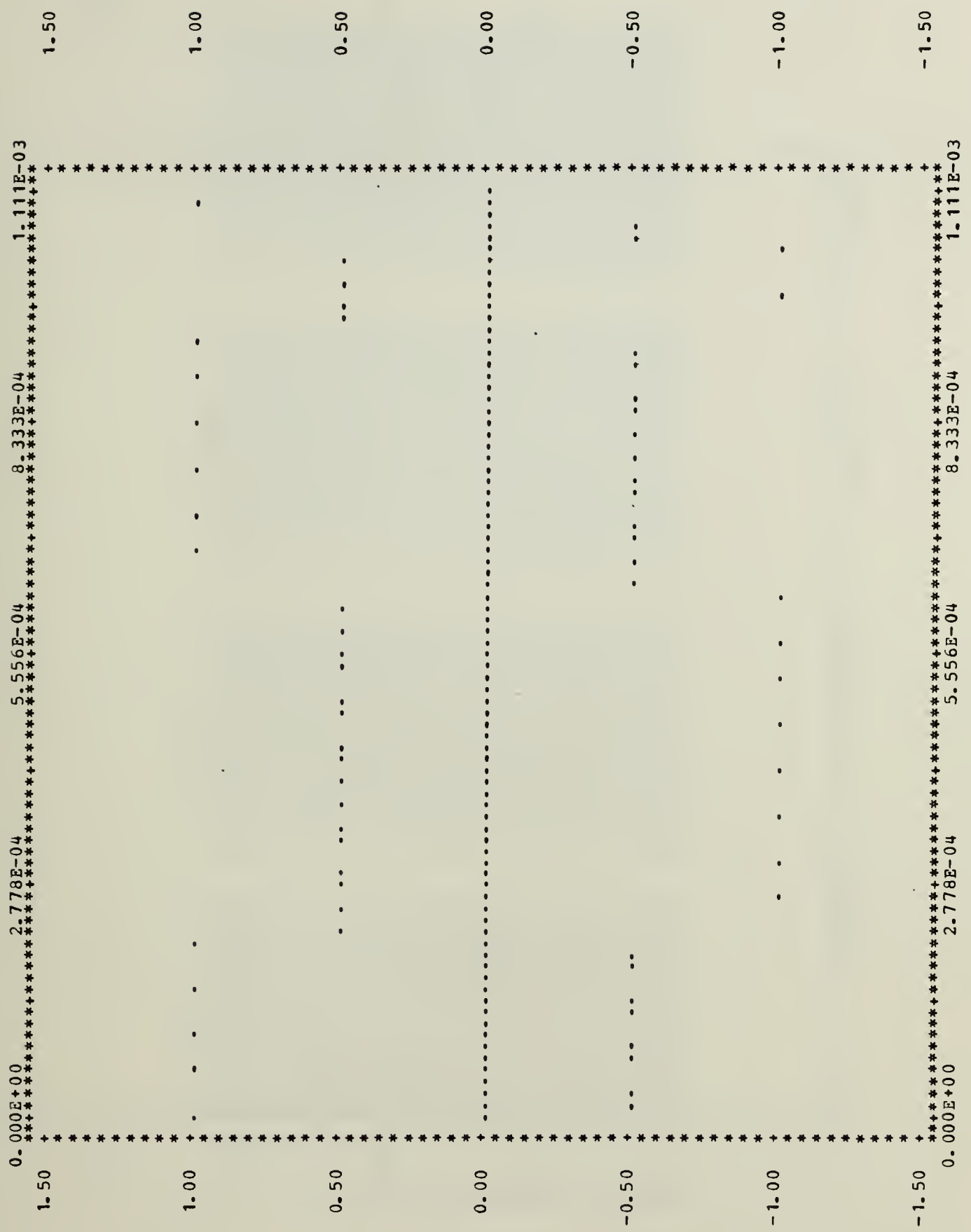
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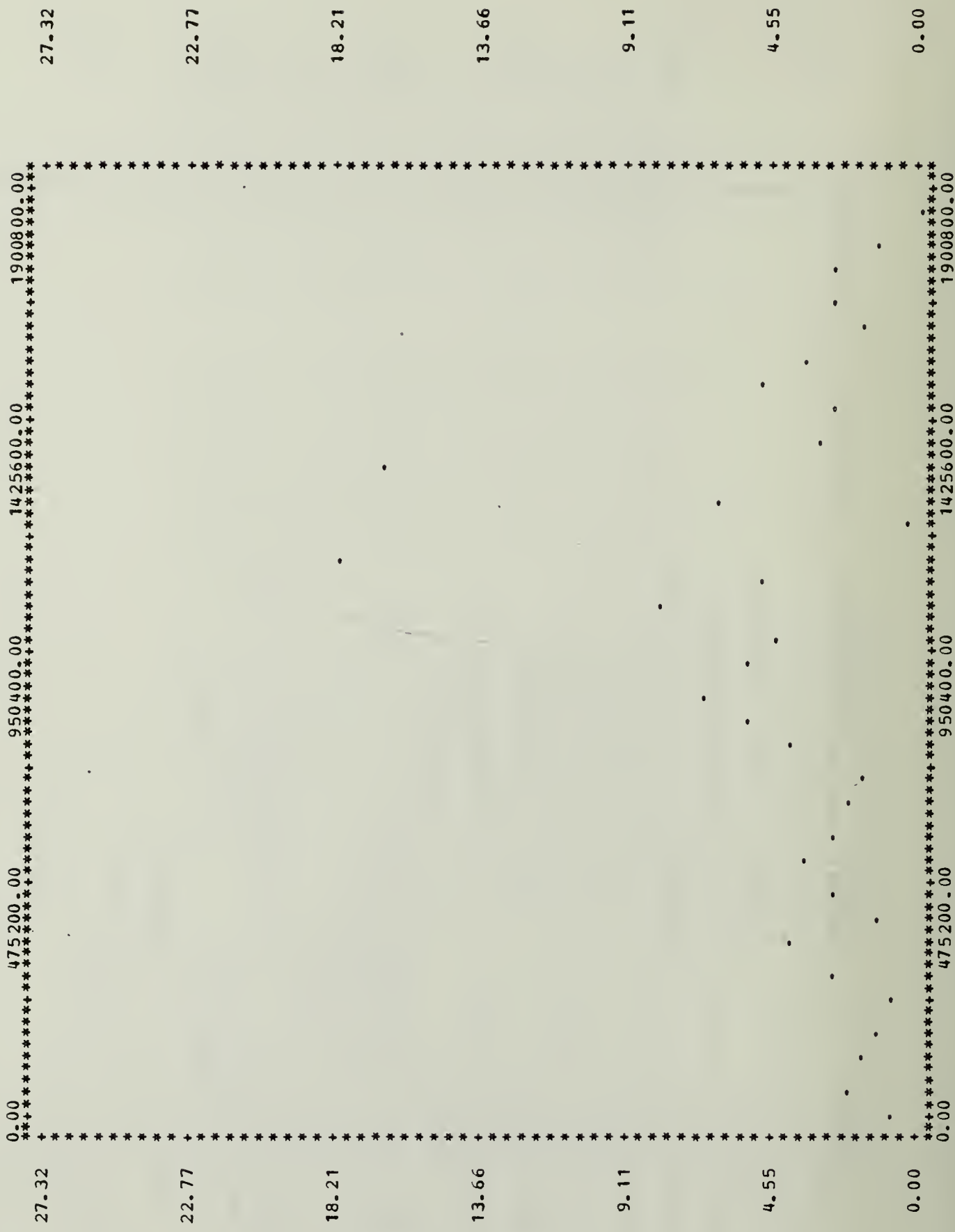
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MODULATION TECHNIQUE = QPSK
BIFOLAR LOGIC

BAUD OR SYMBOL RATE = 1200 HZ

BITS PER BINARY CODE WORD = 2

BIT RATE = 0.2400000000000000E+04

CARRIER FREQUENCY = 2400 HZ

MAXIMUM CARRIER AMPLITUDE = 1 VOLT(S)

INITIAL PHASE ANGLE = 0 DEGREES

TIME BETWEEN SAMPLES = 0.13888888888888889E-03 SEC

NUMBER OF SAMPLES GENERATED = 64

SEED FOR RANDOM NUMBER GENERATOR = 1

NUMBER OF TIMES SIMULATION REPEATS = 100

SUM OF VARIANCES SUM OF VARIANCES**2

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SUM OF SKEWNESS SUM OF SKEWNESS**2

-0.2867982085342969E+05 0.7352270919634266E+08

SUM OF KURTOSIS SUM OF KURTOSIS**2

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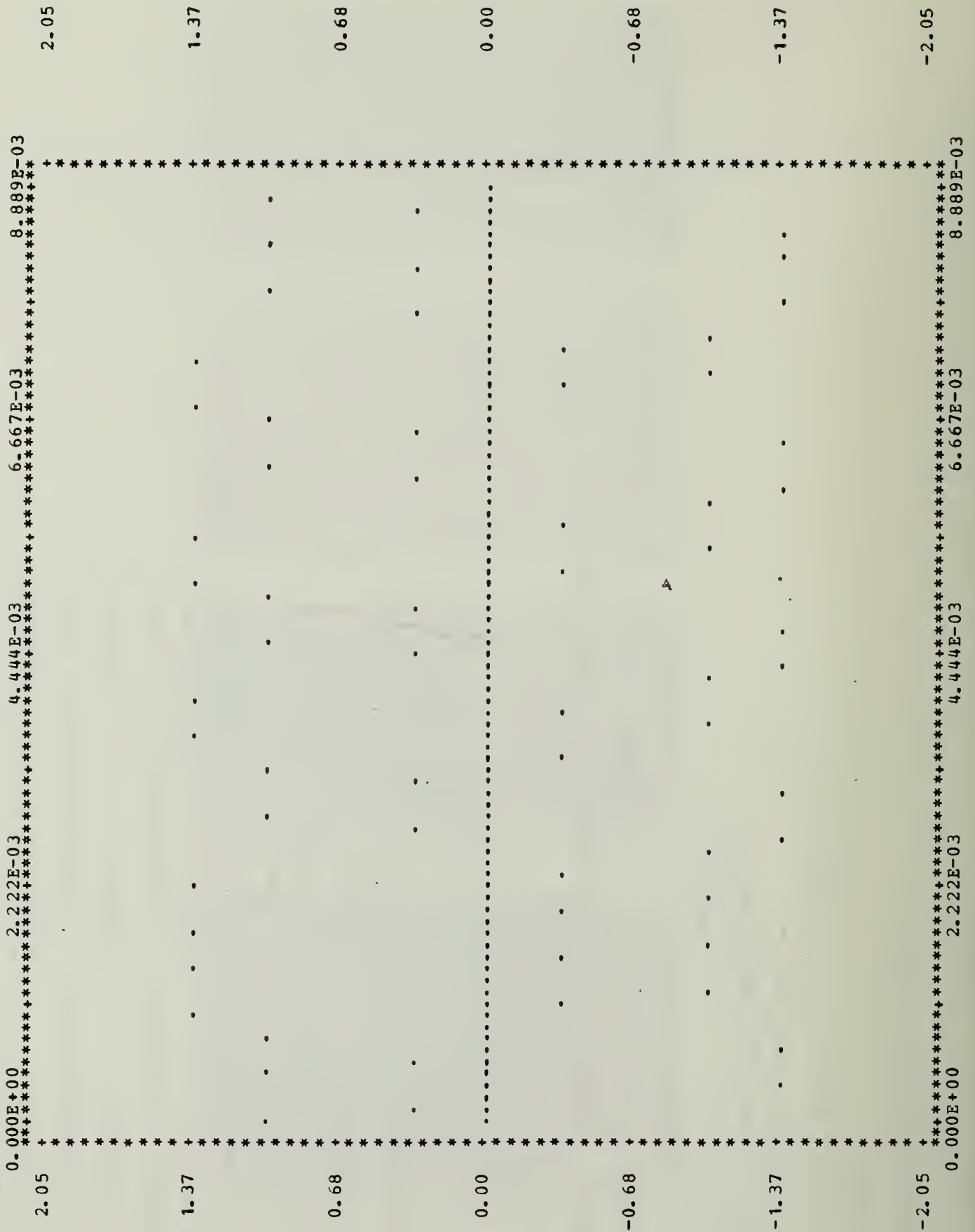
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MEAN SKEWNESS VARIANCE OF THE SKEWNESS

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MEAN KURTOSIS VARIANCE OF THE KURTOSIS

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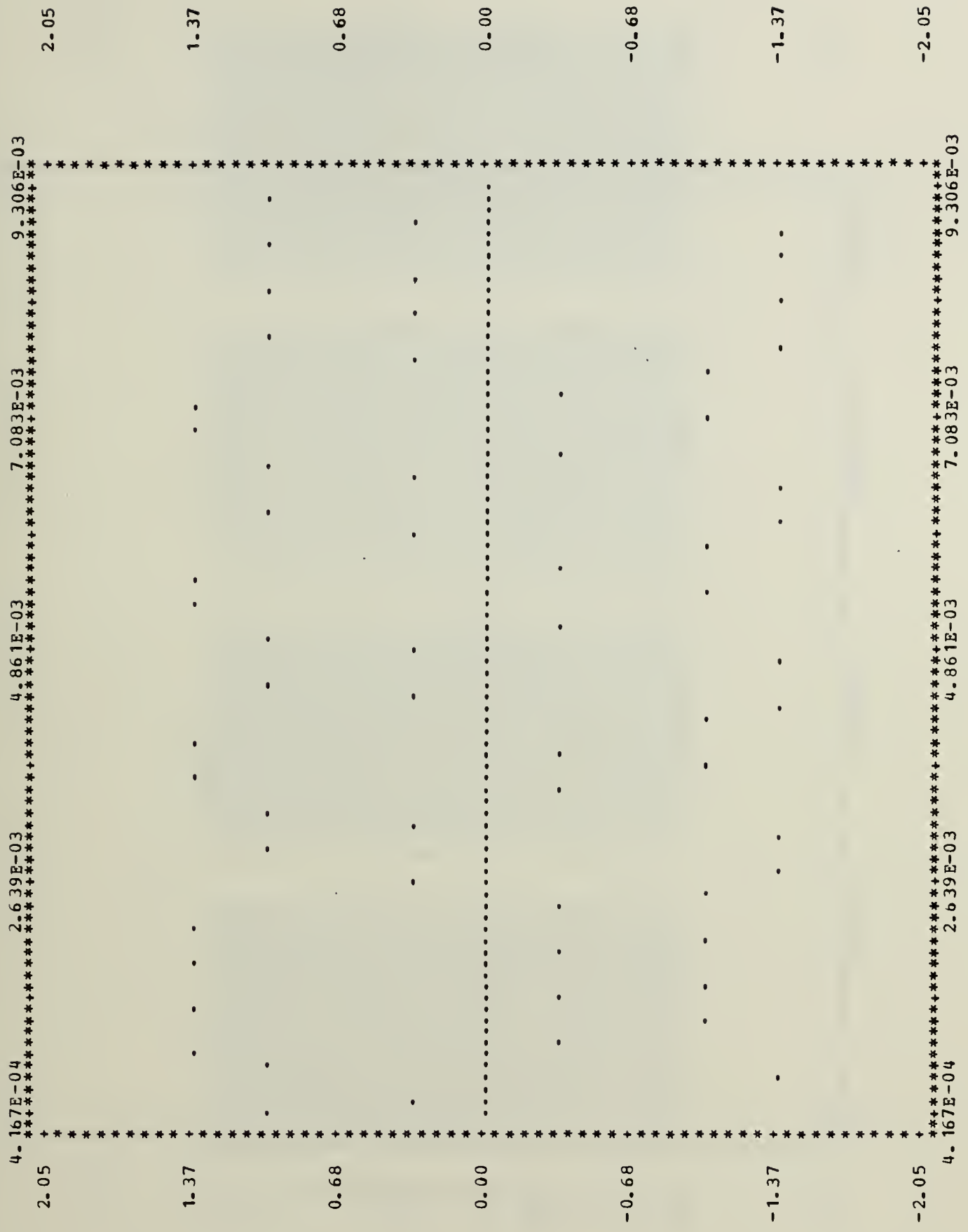




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6	99999	11452	33093	10002
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10	99999	27973	7748E+01	22022
11	99999	34578	9391E+01	22022
12	99999	42933	1121E+01	22022
13	99999	52537	1342E+01	22022
14	99999	63599	1574E+01	22022
15	99999	75223	1816E+01	22022
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17	99999	10028	2332E+01	22022
18	99999	11364	2616E+01	22022
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25	99999	22378	4834E+01	22022
26	99999	24191	5183E+01	22022
27	99999	26064	5540E+01	22022
28	99999	27997	5905E+01	22022
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57	99999	85994	19906E+01	22022
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N	X	X**2	X**3	X**4
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2	9998	9996	9994	9992
3	9997	9994	9991	9988
4	9996	9992	9988	9984
5	9995	9990	9985	9980
6	9994	9988	9982	9976
7	9993	9986	9979	9972
8	9992	9984	9976	9968
9	9991	9982	9973	9964
10	9990	9980	9970	9960
11	9989	9978	9967	9956
12	9988	9976	9964	9952
13	9987	9974	9961	9948
14	9986	9972	9958	9944
15	9985	9970	9955	9940
16	9984	9968	9952	9936
17	9983	9966	9949	9932
18	9982	9964	9946	9928
19	9981	9962	9943	9924
20	9980	9960	9940	9920
21	9979	9958	9937	9916
22	9978	9956	9934	9912
23	9977	9954	9931	9908
24	9976	9952	9928	9904
25	9975	9950	9925	9900
26	9974	9948	9922	9896
27	9973	9946	9919	9892
28	9972	9944	9916	9888
29	9971	9942	9913	9884
30	9970	9940	9910	9880
31	9969	9938	9907	9876
32	9968	9936	9904	9872
33	9967	9934	9901	9868
34	9966	9932	9898	9864
35	9965	9930	9895	9860
36	9964	9928	9892	9856
37	9963	9926	9889	9852
38	9962	9924	9886	9848
39	9961	9922	9883	9844
40	9960	9920	9880	9840
41	9959	9918	9877	9836
42	9958	9916	9874	9832
43	9957	9914	9871	9828
44	9956	9912	9868	9824
45	9955	9910	9865	9820
46	9954	9908	9862	9816
47	9953	9906	9859	9812
48	9952	9904	9856	9808
49	9951	9902	9853	9804
50	9950	9900	9850	9800
51	9949	9898	9847	9796
52	9948	9896	9844	9792
53	9947	9894	9841	9788
54	9946	9892	9838	9784
55	9945	9890	9835	9780
56	9944	9888	9832	9776
57	9943	9886	9829	9772
58	9942	9884	9826	9768
59	9941	9882	9823	9764
60	9940	9880	9820	9760
61	9939	9878	9817	9756
62	9938	9876	9814	9752
63	9937	9874	9811	9748
64	9936	9872	9808	9744
65	9935	9870	9805	9740
66	9934	9868	9802	9736
67	9933	9866	9799	9732
68	9932	9864	9796	9728
69	9931	9862	9793	9724
70	9930	9860	9790	9720
71	9929	9858	9787	9716
72	9928	9856	9784	9712
73	9927	9854	9781	9708
74	9926	9852	9778	9704
75	9925	9850	9775	9700
76	9924	9848	9772	9696
77	9923	9846	9769	9692
78	9922	9844	9766	9688
79	9921	9842	9763	9684
80	9920	9840	9760	9680
81	9919	9838	9757	9676
82	9918	9836	9754	9672
83	9917	9834	9751	9668
84	9916	9832	9748	9664
85	9915	9830	9745	9660
86	9914	9828	9742	9656
87	9913	9826	9739	9652
88	9912	9824	9736	9648
89	9911	9822	9733	9644
90	9910	9820	9730	9640
91	9909	9818	9727	9636
92	9908	9816	9724	9632
93	9907	9814	9721	9628
94	9906	9812	9718	9624
95	9905	9810	9715	9620
96	9904	9808	9712	9616
97	9903	9806	9709	9612
98	9902	9804	9706	9608
99	9901	9802	9703	9604
100	9900	9800	9700	9600

MODULATION TECHNIQUE = OQPSK
 BIFOLAR LOGIC
 BAUD OR SYMBOL RATE = 1200 HZ
 BITS PER BINARY CODE WORD = 2
 BIT RATE = 0.2400000000000000E+04
 CARRIER FREQUENCY = 2400 HZ
 MAXIMUM CARRIER AMPLITUDE = 1 VOLT(S)
 INITIAL PHASE ANGLE = 0 DEGREES
 TIME BETWEEN SAMPLES = 0.1388888888888889E-03 SEC
 NUMBER OF SAMPLES GENERATED = 64
 SEED FOR RANDOM NUMBER GENERATOR = 1
 NUMBER OF TIMES SIMULATION REPEATS = 100
 SUM OF VARIANCES SUM OF VARIANCES**2
 0.4302799744926702E+03 0.1192673508267923E+05
 SUM OF SKEWNESS SUM OF SKEWNESS**2
 -0.2766466990808353E+05 0.6316161942013623E+08
 SUM OF KURTOSIS SUM OF KURTOSIS**2
 0.3332128031283272E+05 0.9992700833249297E+08
 MEAN VARIANCE VARIANCE OF THE VARIANCES
 0.1303878710583849E+02 0.1973876906051148E+03
 MEAN SKEWNESS VARIANCE OF THE SKEWNESS
 -0.8383233305479857E+03 0.1249052537633781E+07
 MEAN KURTOSIS VARIANCE OF THE KURTOSIS
 0.1009735767055537E+04 0.2071291243641945E+07

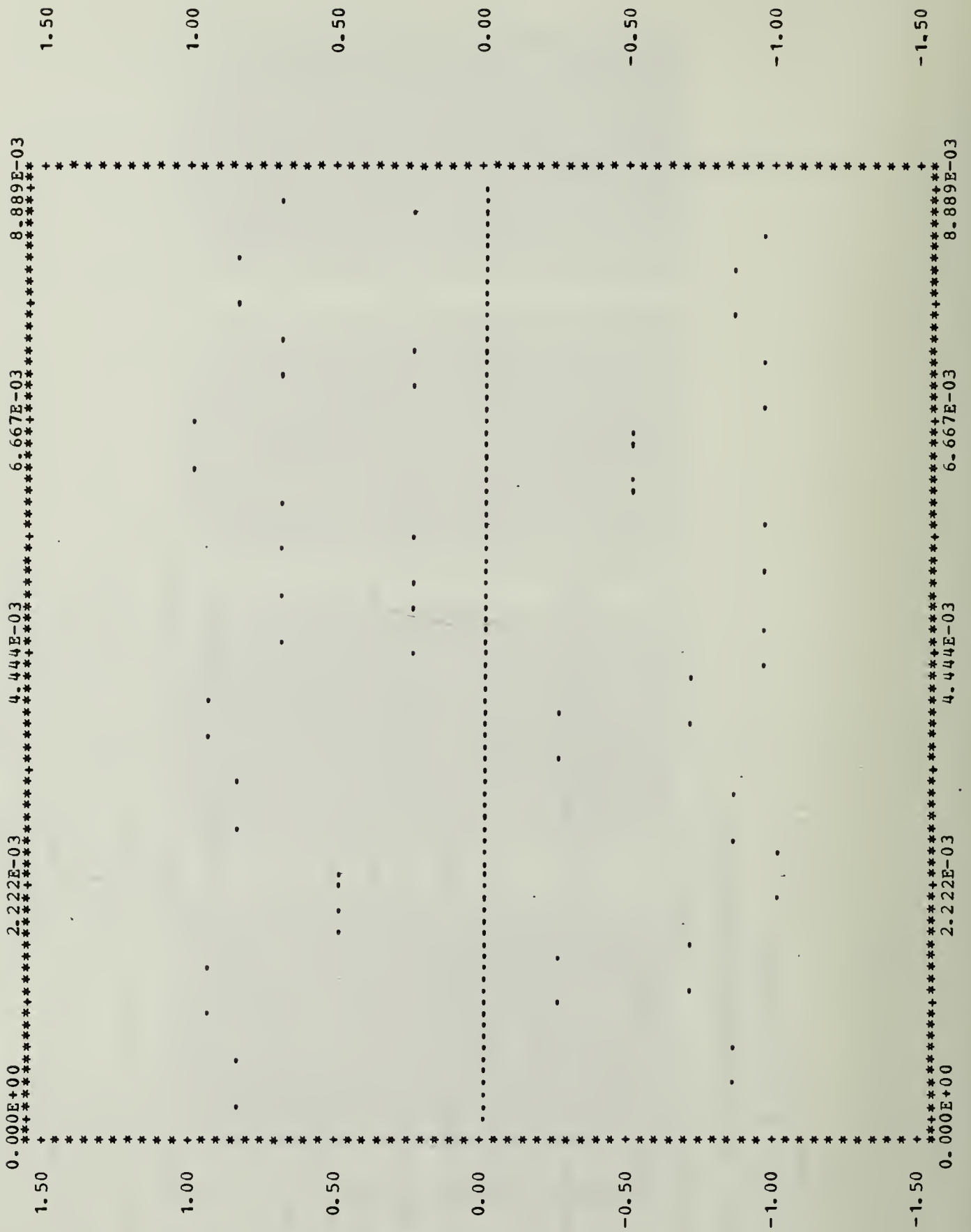




N	MEAN	VARIANCE	SKENWNESS	KURTOSIS
1	999999999	1561758578800	1598721155466	2664533525910
2	1372323826	406867864354	13863769226752	404181597538670
3	2001396615	9269424591664	773336583896700	18623228726701
4	2772862445	1678068152390	2623023671424	8004509154646
5	3777641084	2932577358584	668530129499	2588931213699
6	3829098409	4020832039397	558748996021	3918832866508
7	2961659942	3191184357736	727242587407	261250589140
8	2148359327	1733213354178	175456869710	111359743383
9	1345271169	106083134373	293038830923	252297496663
10	1227933390	419727640110	253057703330	471760743450
11	2439525645	505444768471	720754700969	366540306408
12	3624460779	178142066874	88289360955	949060006845
13	5344290929	295816570632	57803973417	299239402240
14	6817466815	870744263584	27526112331	233689660905
15	7712888151	247490289239	53512655639	171328115026
16	9428086215	193161505542	93895599099	190613260058
17	1072214978	280507286944	70236620891	89265702024
18	1081933825	344085141546	85062282026	18389337522
19	1199506255	358000181133	10660342212	29317768352
20	1128041374	344377191596	20505032027	35763292721
21	1239679866	39768668800	37255715577	28128181268
22	1194093966	32282743096	72557168916	52815369433
23	9561857571	35120704299	8117741011	31797176964
24	1060742458	25439111774	6039916572	30093532031
25	8728674900	313975308059	7620482666	18741237839
26	6256141872	46686849452	23438960001	28060956913
27	3639693642	12112099312	63438260618	20167934198
28	3386927083	57477787324	3793167844	44877667872
29	1732050807	13995152269	8233410774	77816705472
30	999999999	00000000000	92330484540	274640706699
31	999999999	00000000000	92330484540	274640706699
32	999999999	00000000000	92330484540	274640706699
33	999999999	00000000000	92330484540	274640706699

N	Y	SUM	X**2	X**3	X**4
1	9999	9999	9999	9999	9999
2	9999	9999	9999	9999	9999
3	9999	9999	9999	9999	9999
4	9999	9999	9999	9999	9999
5	9999	9999	9999	9999	9999
6	9999	9999	9999	9999	9999
7	9999	9999	9999	9999	9999
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15	9999	9999	9999	9999	9999
16	9999	9999	9999	9999	9999
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18	9999	9999	9999	9999	9999
19	9999	9999	9999	9999	9999
20	9999	9999	9999	9999	9999
21	9999	9999	9999	9999	9999
22	9999	9999	9999	9999	9999
23	9999	9999	9999	9999	9999
24	9999	9999	9999	9999	9999
25	9999	9999	9999	9999	9999
26	9999	9999	9999	9999	9999
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28	9999	9999	9999	9999	9999
29	9999	9999	9999	9999	9999
30	9999	9999	9999	9999	9999
31	9999	9999	9999	9999	9999
32	9999	9999	9999	9999	9999
33	9999	9999	9999	9999	9999

MODULATION TECHNIQUE = MPSK
 BIFOLAR LOGIC
 BAUD OR SYMBOL RATE = 1200 HZ
 BITS PER BINARY CODE WORD = 3
 BIT RATE = 0.3600000000000000E+04
 CARRIER FREQUENCY = 2400 HZ
 MAXIMUM CARRIER AMPLITUDE = 1 VOLT(S)
 INITIAL PHASE ANGLE = 0 DEGREES
 TIME BETWEEN SAMPLES = 0.1388888888888889E-03 SEC
 NUMBER OF SAMPLES GENERATED = 64
 SEED FOR RANDOM NUMBER GENERATOR = 1
 NUMBER OF TIMES SIMULATION REPEATS = 100
 SUM OF VARIANCES SUM OF VARIANCES**2
 0.2100020931141337E+03 0.2899383925937582E+04
 SUM OF SKEWNESS SUM OF SKEWNESS**2
 -0.960095280888690E+04 0.8204154937490084E+07
 SUM OF KURTOSIS SUM OF KURTOSIS**2
 0.8272550682771584E+04 0.7152001918873632E+07
 MEAN VARIANCE VARIANCE OF THE VARIANCES
 0.6363699791337385E+01 0.4884355155646109E+02
 MEAN SKEWNESS VARIANCE OF THE SKEWNESS
 -0.2909392509360209E+03 0.1690890175696266E+06
 MEAN KURTOSIS VARIANCE OF THE KURTOSIS
 0.2506833540233813E+03 0.1586940989808761E+06

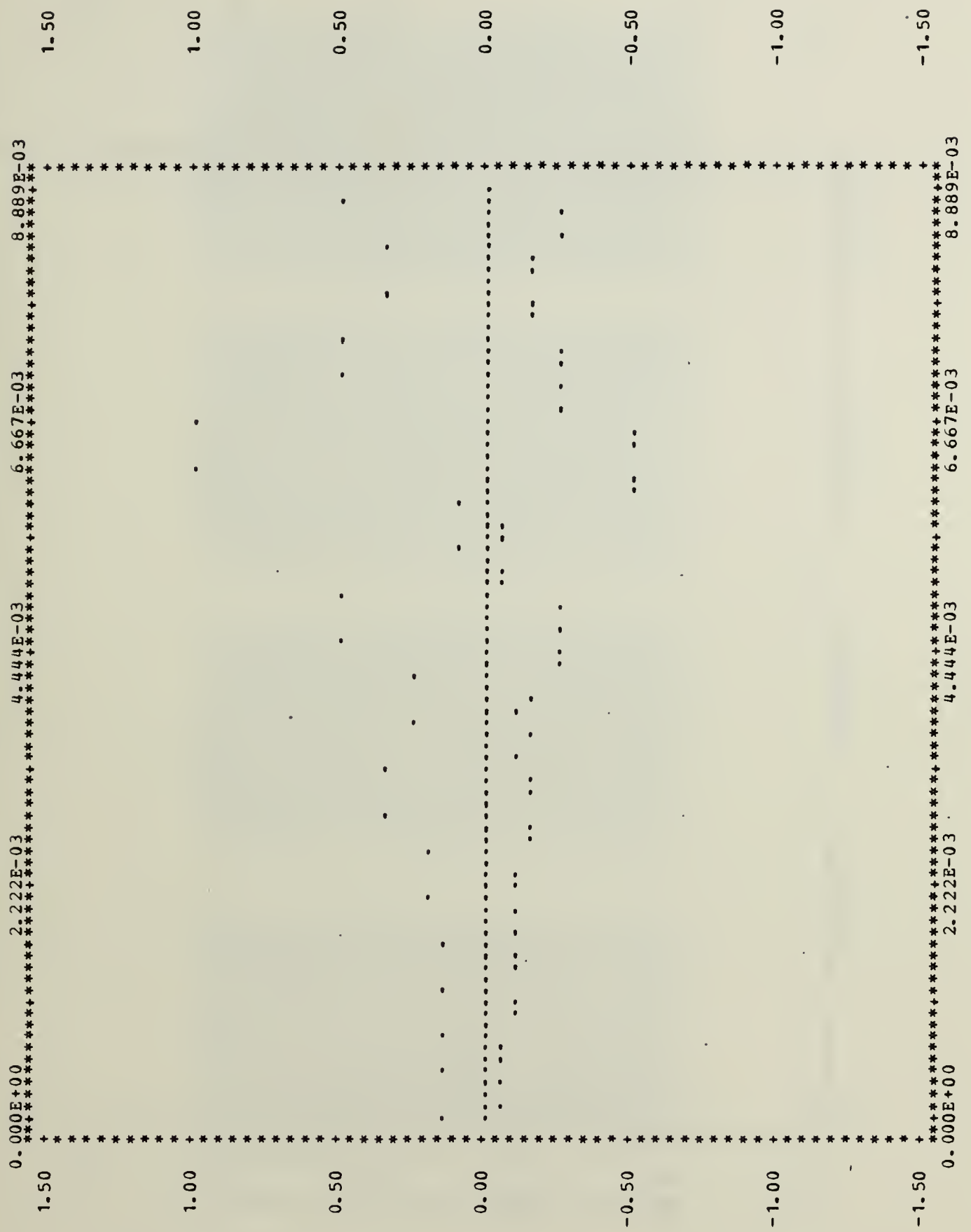


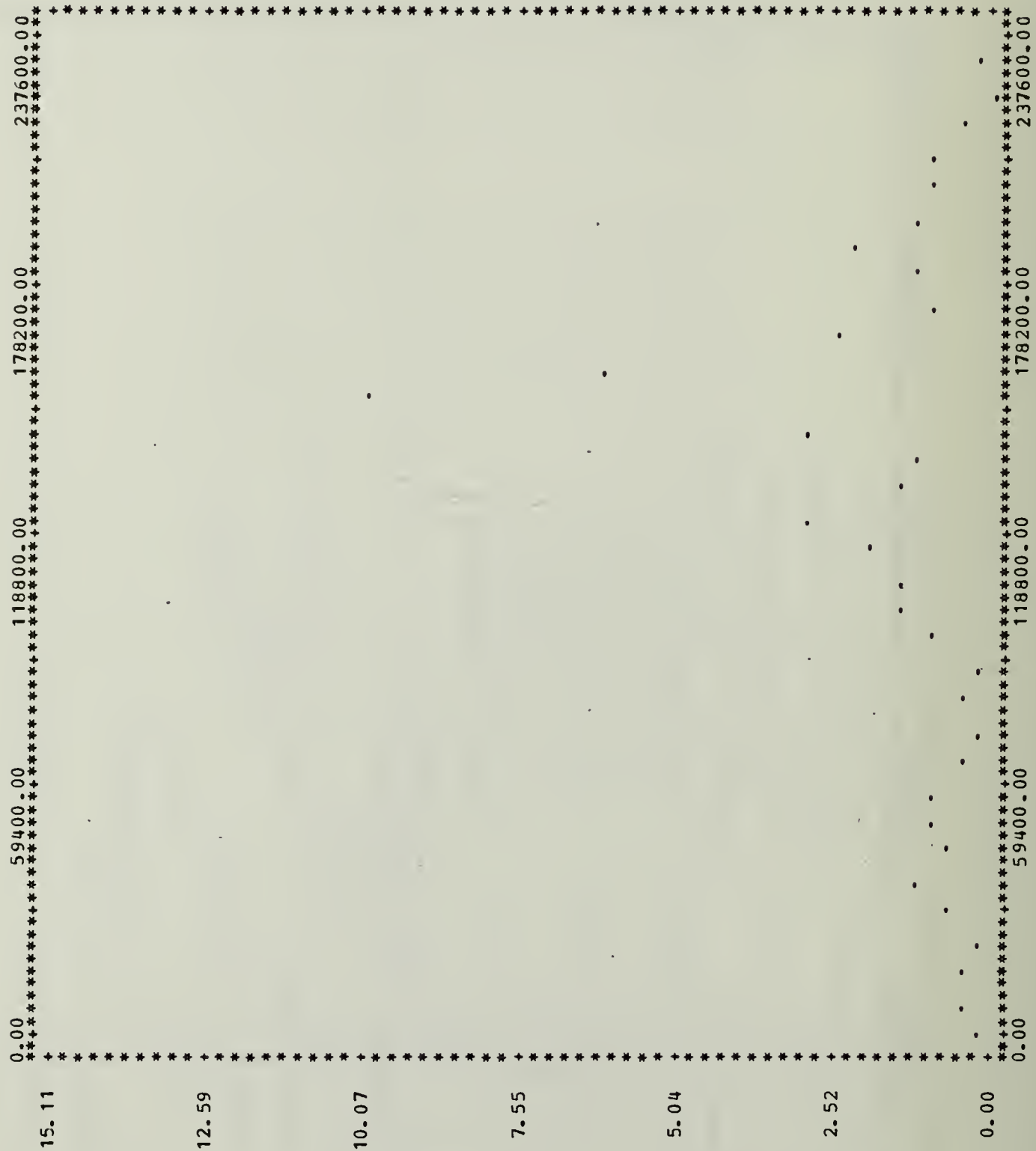


N	MEAN	VARIANCE	STANDARD DEVIATION	KURTOSIS
1	5852	1489	38.46	4.06
2	8991	3368	58.04	5.67
3	1277	9520	97.56	16.96
4	1737	3563	59.70	22.55
5	2121	9751	98.74	33.32
6	2424	2378	48.67	16.06
7	2493	4077	63.84	22.78
8	2478	8045	89.65	33.44
9	2071	5933	77.06	26.72
10	1792	2658	51.48	15.55
11	1338	4219	64.95	22.00
12	1206	7941	89.15	33.33
13	1701	0792	28.33	10.66
14	2834	1506	38.82	18.45
15	3743	8055	89.74	33.33
16	4661	6488	80.55	28.28
17	6706	9089	95.33	38.66
18	7233	5281	72.66	28.28
19	8344	4759	68.82	26.72
20	8944	6234	78.94	33.33
21	8814	7839	88.54	33.33
22	8749	5097	71.48	28.28
23	8285	9821	99.60	40.00
24	7248	4188	64.66	22.55
25	6582	0180	42.33	13.80
26	5574	4269	65.33	22.55
27	4540	9600	98.00	38.66
28	3600	8233	90.72	33.33
29	2979	6323	79.54	28.28
30	1788	7726	87.85	33.33
31	1438	8925	94.57	38.66
32	1193	4583	67.70	26.72
33	9317	5834	76.41	33.33
34	1160	7564	86.99	33.33
35	5834	1956	44.27	15.55
36	2186	330E+00	57.50	22.55
37	2949	0253	50.4E+00	16.06
38	1477	8479	92.77	33.33
39	1246	9250	66.33	26.72
40	2098	1453	38.46	15.55
41	1038	0709	26.72	10.66
42	8172	2058	45.33	18.45
43	4602	4103	64.27	28.28
44	3465	1460	38.46	15.55
45	8240	0341	58.33	22.55
46	1823	8055	89.74	33.33
47	3670	9112	106.66	40.00
48	5878	2247	76.41	33.33
49	7336	8433	91.70	38.66
50	1179	0564	76.41	33.33
51	2143	3264	56.99	22.55
52	1849	5434	73.21	28.28
53	1838	6598	81.11	33.33
54	1666	4039	63.84	26.72
55	8177	6355	79.77	33.33
56	6531	1450	38.46	15.55
57	2838	9880	99.41	40.00
58	2494	3350	57.85	22.55
59	8979	9177	95.66	38.66
60	7161	1261	35.33	13.80
61	4955	5334	73.21	28.28
62	1959	1760	41.91	16.06
63	3929	8053	89.74	33.33
64	6936	7429	86.27	33.33
65	1477	8479	92.77	33.33
66	1246	9250	66.33	26.72
67	2098	1453	38.46	15.55
68	1038	0709	26.72	10.66
69	8172	2058	45.33	18.45
70	4602	4103	64.27	28.28
71	3465	1460	38.46	15.55
72	8240	0341	58.33	22.55
73	1823	8055	89.74	33.33
74	3670	9112	106.66	40.00
75	5878	2247	76.41	33.33
76	7336	8433	91.70	38.66
77	1179	0564	76.41	33.33
78	2143	3264	56.99	22.55
79	1849	5434	73.21	28.28
80	1838	6598	81.11	33.33
81	1666	4039	63.84	26.72
82	8177	6355	79.77	33.33
83	6531	1450	38.46	15.55
84	2838	9880	99.41	40.00
85	2494	3350	57.85	22.55
86	8979	9177	95.66	38.66
87	7161	1261	35.33	13.80
88	4955	5334	73.21	28.28
89	1959	1760	41.91	16.06
90	3929	8053	89.74	33.33
91	6936	7429	86.27	33.33
92	1477	8479	92.77	33.33
93	1246	9250	66.33	26.72
94	2098	1453	38.46	15.55
95	1038	0709	26.72	10.66
96	8172	2058	45.33	18.45
97	4602	4103	64.27	28.28
98	3465	1460	38.46	15.55
99	8240	0341	58.33	22.55
100	1823	8055	89.74	33.33

N	X	Y	SUM	X**3	X**2	Y**2	XY	SUM	X**3	X**2	Y**2	XY	SUM	X**4	X**3	Y**3	XY
1	1	4	585	1	1	16	4	4	1	1	16	4	4	1	1	64	4
2	2	9	899	8	4	81	18	11	4	16	162	36	16	8	8	729	18
3	3	14	1279	27	9	196	42	20	9	25	392	84	20	27	27	2744	42
4	4	19	1737	64	16	361	76	27	16	36	676	144	27	64	64	6859	76
5	5	24	2121	125	25	576	120	35	25	49	1024	240	35	125	125	14744	120
6	6	29	2493	216	36	841	174	45	36	64	1444	360	45	216	216	21681	174
7	7	34	2843	343	49	1156	238	55	49	81	2016	476	55	343	343	42196	238
8	8	39	3171	512	64	1521	312	65	64	100	2721	672	65	512	512	59319	312
9	9	44	3479	729	81	1936	396	77	81	121	3544	936	77	729	729	77824	396
10	10	49	3767	1000	100	2401	490	89	100	144	4410	1260	89	1000	1000	10000	490
11	11	54	4035	1331	121	2916	594	97	121	169	5284	1638	97	1331	1331	13310	594
12	12	59	4283	1728	144	3481	702	105	144	196	6184	1944	105	1728	1728	17280	702
13	13	64	4511	2197	169	4096	816	113	169	225	7144	2316	113	2197	2197	21970	816
14	14	69	4719	2744	196	4761	930	121	196	256	8244	2706	121	2744	2744	27440	930
15	15	74	4907	3375	225	5476	1050	127	225	289	9344	3150	127	3375	3375	33750	1050
16	16	79	5075	4096	256	6241	1176	133	256	324	10440	3528	133	4096	4096	40960	1176
17	17	84	5223	4913	289	7056	1302	139	289	361	11544	3918	139	4913	4913	49130	1302
18	18	89	5351	5832	324	7921	1428	145	324	396	12640	4212	145	5832	5832	58320	1428
19	19	94	5469	6859	361	8836	1554	151	361	436	13744	4518	151	6859	6859	68590	1554
20	20	99	5577	8000	400	9801	1680	157	400	481	14840	4836	157	8000	8000	80000	1680
21	21	104	5675	9261	441	10816	1806	163	441	524	15944	5142	163	9261	9261	92610	1806
22	22	109	5763	10648	484	11841	1932	169	484	569	17040	5458	169	10648	10648	106480	1932
23	23	114	5841	12167	529	12884	2058	175	529	616	18144	5784	175	12167	12167	121670	2058
24	24	119	5909	13824	576	13941	2184	181	576	665	19240	6120	181	13824	13824	138240	2184
25	25	124	5967	15625	625	15004	2310	187	625	716	20344	6466	187	15625	15625	156250	2310
26	26	129	6015	17568	676	16081	2436	193	676	769	21440	6822	193	17568	17568	175680	2436
27	27	134	6063	19659	729	17176	2562	199	729	824	22544	7188	199	19659	19659	196590	2562
28	28	139	6101	21896	784	18289	2688	205	784	881	23640	7594	205	21896	21896	218960	2688
29	29	144	6139	24287	841	19424	2814	211	841	940	24744	8010	211	24287	24287	242870	2814
30	30	149	6177	26834	900	20581	2940	217	900	1001	25840	8436	217	26834	26834	268340	2940
31	31	154	6215	29539	961	21756	3066	223	961	1064	26944	8882	223	29539	29539	295390	3066
32	32	159	6253	32400	1024	22956	3192	229	1024	1129	28040	9338	229	32400	32400	324000	3192
33	33	164	6291	35427	1089	24181	3318	235	1089	1196	29144	9804	235	35427	35427	354270	3318

MODULATION TECHNIQUE = MASK
 BIFOLAR LOGIC
 BAUD OR SYMBOL RATE = 1200 HZ
 BITS PER BINARY CODE WORD = 3
 BIT RATE = 0.3600000000000000E+04
 CARRIER FREQUENCY = 2400 HZ
 MAXIMUM CARRIER AMPLITUDE = 1 VOLT(S)
 INITIAL PHASE ANGLE = 0 DEGREES
 TIME BETWEEN SAMPLES = 0.13888888888888889E-03 SEC
 NUMBER OF SAMPLES GENERATED = 64
 SEED FOR RANDOM NUMBER GENERATOR = 1
 NUMBER OF TIMES SIMULATION REPEATS = 100
 SUM OF VARIANCES SUM OF VARIANCES**2
 0.2672011399771625E+02 0.6236464612091026E+02
 SUM OF SKEWNESS SUM OF SKEWNESS**2
 -0.1657760855944905E+04 0.1880354503890174E+07
 SUM OF KURTOSIS SUM OF KURTOSIS**2
 0.1906467874763258E+03 0.7184370776848387E+04
 MEAN VARIANCE VARIANCE OF THE VARIANCES
 0.8097004241732196E+00 0.1272792452593831E+01
 MEAN SKEWNESS VARIANCE OF THE SKEWNESS
 -0.5023517745287592E+02 0.5615864353491720E+05
 MEAN KURTOSIS VARIANCE OF THE KURTOSIS
 0.5777175378070478E+01 0.1900928390728725E+03

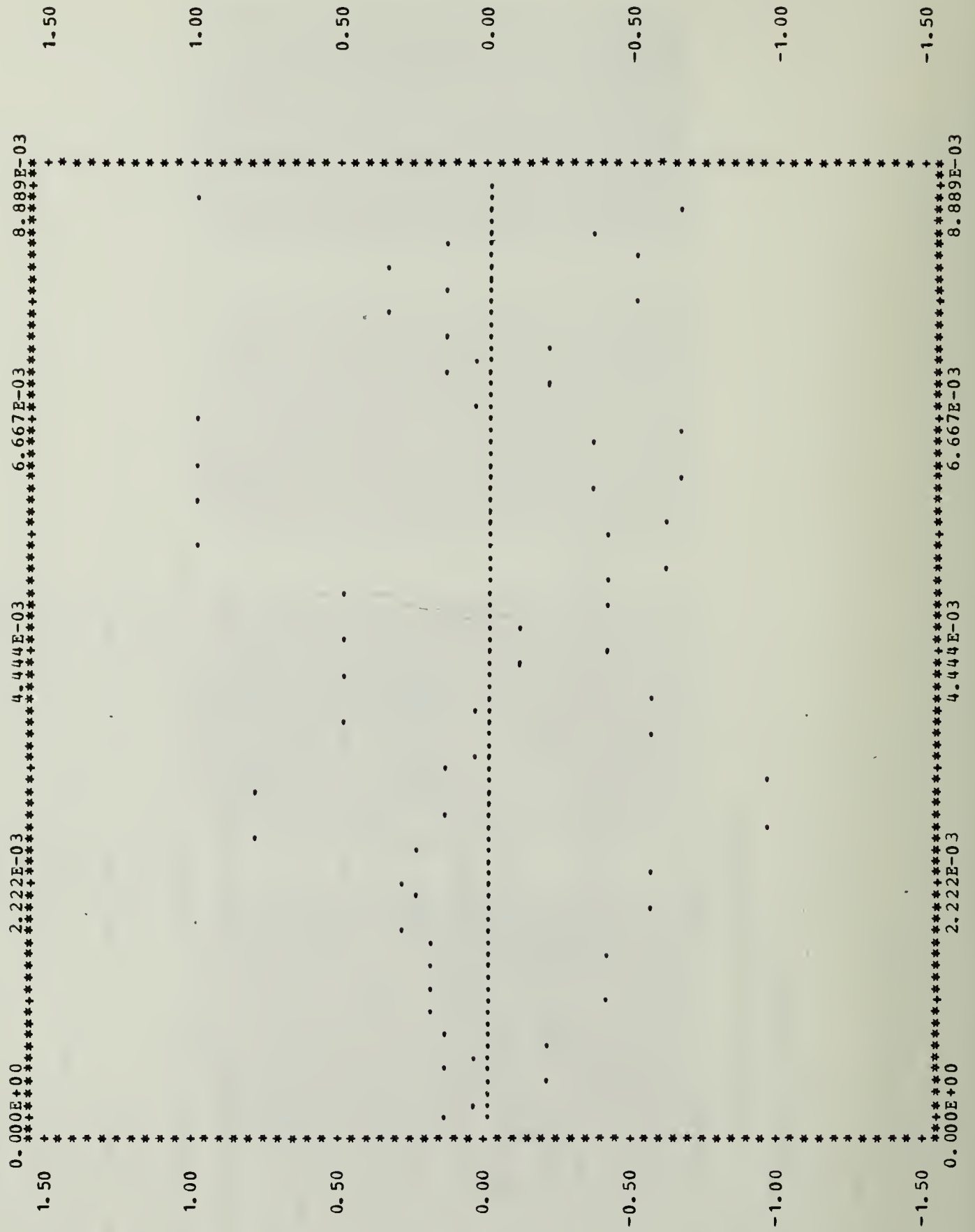


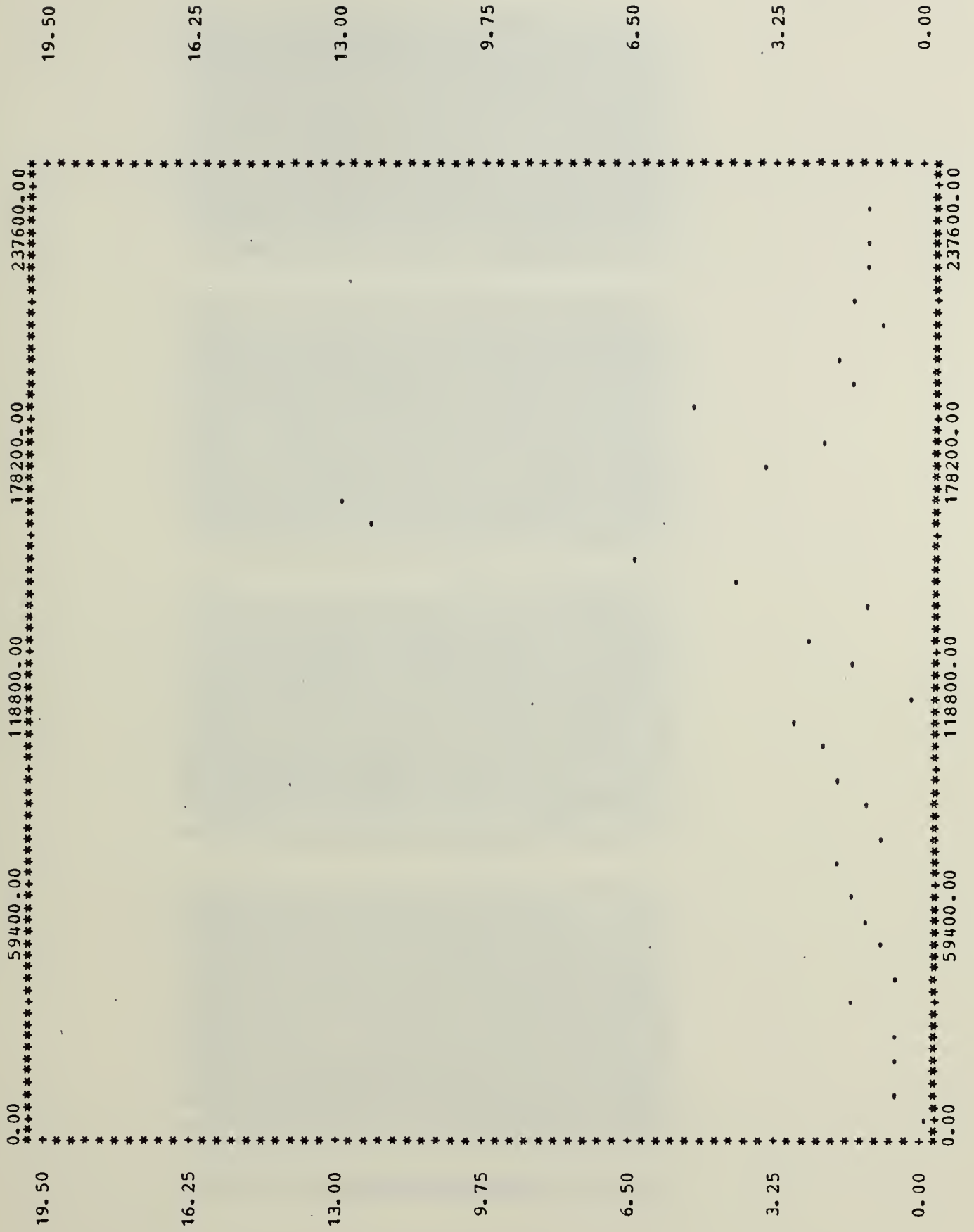


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MEAN	339	339	339	339	339	339	339	339	339	339	339	339	339	339	339	339	339	339	339	339	339	339	339	339	339	339	339	339	339	339	339	339	339
VARIANCE	8384	7668	7847	1013	5050	6697	5804	1582	2475	4455	1857	1626	4634	5941	5941	3319	2299	7062	1357	1242	3566	5536	8493	2279	1317	8497	7665	1515	2806	1763	8431	3965	8905
KEYMEANS	1893	2283	3309	3343	3343	3343	3343	3343	3343	3343	3343	3343	3343	3343	3343	3343	3343	3343	3343	3343	3343	3343	3343	3343	3343	3343	3343	3343	3343	3343	3343	3343	3343
URTOSTS	2742	2891	1556	1048	1090	8553	3369	2119	2119	2119	2119	2119	2119	2119	2119	2119	2119	2119	2119	2119	2119	2119	2119	2119	2119	2119	2119	2119	2119	2119	2119	2119	2119

N	X	SUM	X**2	SUM	X**3	SUM	X**4
1	1	1	1	1	1	1	1
2	2	4	4	8	8	16	16
3	3	9	9	27	27	81	81
4	4	16	16	64	64	256	256
5	5	25	25	125	125	625	625
6	6	36	36	216	216	1296	1296
7	7	49	49	343	343	2401	2401
8	8	64	64	512	512	4096	4096
9	9	81	81	729	729	5904	5904
10	10	100	100	1000	1000	10000	10000
11	11	121	121	1331	1331	14641	14641
12	12	144	144	1728	1728	20736	20736
13	13	169	169	2197	2197	28549	28549
14	14	196	196	2744	2744	37000	37000
15	15	225	225	3375	3375	47250	47250
16	16	256	256	4096	4096	58976	58976
17	17	289	289	4913	4913	72601	72601
18	18	324	324	5832	5832	89472	89472
19	19	361	361	6859	6859	109271	109271
20	20	400	400	8000	8000	132000	132000
21	21	441	441	9261	9261	158761	158761
22	22	484	484	10648	10648	189808	189808
23	23	529	529	12167	12167	225747	225747
24	24	576	576	13824	13824	266880	266880
25	25	625	625	15625	15625	313625	313625
26	26	676	676	17568	17568	366464	366464
27	27	729	729	19659	19659	425947	425947
28	28	784	784	21904	21904	492224	492224
29	29	841	841	24309	24309	565841	565841
30	30	900	900	26880	26880	648000	648000
31	31	961	961	29611	29611	739041	739041
32	32	1024	1024	32512	32512	838016	838016
33	33	1089	1089	35583	35583	944949	944949

MODULATION TECHNIQUE = QASK
 BIFOLAR LOGIC
 BAUD OR SYMBOL RATE = 1200 HZ
 BITS PER BINARY CODE WORD = 3
 BIT RATE = 0.3600000000000000E+04
 CARRIER FREQUENCY = 2400 HZ
 MAXIMUM CARRIER AMPLITUDE = 1 VOLT(S)
 INITIAL PHASE ANGLE = 0 DEGREES
 TIME BETWEEN SAMPLES = 0.1388888888888889E-03 SEC
 NUMBER OF SAMPLES GENERATED = 64
 SEED FOR RANDOM NUMBER GENERATOR = 1
 NUMBER OF TIMES SIMULATION REPEATS = 100
 SUM OF VARIANCES SUM OF VARIANCES**2
 0.4885105807865026E+02 0.1949104911522201E+03
 SUM OF SKEWNESS SUM OF SKEWNESS**2
 -0.5438333348597472E+04 0.1951490781083542E+08
 SUM OF KURTOSIS SUM OF KURTOSIS**2
 0.6866043785868234E+03 0.9002560164061202E+05
 MEAN VARIANCE VARIANCE OF THE VARIANCES
 0.1480335093292432E+01 0.3831079860435228E+01
 MEAN SKEWNESS VARIANCE OF THE SKEWNESS
 -0.1647979802605294E+03 0.5818337955938460E+06
 MEAN KURTOSIS VARIANCE OF THE KURTOSIS
 0.2080619329050980E+02 0.2366874319550756E+04





N	MEAN	VARIANCE	SKENNESS	KURTOSIS
1	363.1071	9.100000	4.876444	27.365509
2	427.5657	10.774029	4.444817	30.934642
3	457.8356	10.447298	3.671461	31.481041
4	592.6833	13.986694	2.812110	31.876806
5	625.8633	22.370622	1.777804	45.286947
6	633.5533	24.484208	1.887438	12.591884
7	605.4054	28.219210	1.916932	14.078377
8	615.4661	23.298021	1.914633	12.552525
9	604.1966	25.731603	1.908712	12.538951
10	607.1966	22.573160	1.908712	12.538951
11	607.1966	22.573160	1.908712	12.538951
12	607.1966	22.573160	1.908712	12.538951
13	607.1966	22.573160	1.908712	12.538951
14	607.1966	22.573160	1.908712	12.538951
15	607.1966	22.573160	1.908712	12.538951
16	607.1966	22.573160	1.908712	12.538951
17	607.1966	22.573160	1.908712	12.538951
18	607.1966	22.573160	1.908712	12.538951
19	607.1966	22.573160	1.908712	12.538951
20	607.1966	22.573160	1.908712	12.538951
21	607.1966	22.573160	1.908712	12.538951
22	607.1966	22.573160	1.908712	12.538951
23	607.1966	22.573160	1.908712	12.538951
24	607.1966	22.573160	1.908712	12.538951
25	607.1966	22.573160	1.908712	12.538951
26	607.1966	22.573160	1.908712	12.538951
27	607.1966	22.573160	1.908712	12.538951
28	607.1966	22.573160	1.908712	12.538951
29	607.1966	22.573160	1.908712	12.538951
30	607.1966	22.573160	1.908712	12.538951
31	607.1966	22.573160	1.908712	12.538951
32	607.1966	22.573160	1.908712	12.538951
33	607.1966	22.573160	1.908712	12.538951

MODULATION TECHNIQUE = MSK
BIFOLAR LOGIC

BAUD OR SYMBOL RATE = 1200 HZ

BITS PER BINARY CODE WORD = 1

BIT RATE = 0.1200000000000000E+04

CARRIER FREQUENCY = 3000 HZ

MAXIMUM CARRIER AMPLITUDE = 1 VOLT(S)

INITIAL PHASE ANGLE = 0 DEGREES

TIME BETWEEN SAMPLES = 0.1111111111111111E-03 SEC

NUMBER OF SAMPLES GENERATED = 64

SEED FOR RANDOM NUMBER GENERATOR = 1

NUMBER OF TIMES SIMULATION REPEATS = 100

SUM OF VARIANCES SUM OF VARIANCES**2

0.1525890150844788E+03 0.2084564025759793E+04

SUM OF SKEWNESS SUM OF SKEWNESS**2

-0.1665578258850635E+05 0.9704853819233804E+08

SUM OF KURTOSIS SUM OF KURTOSIS**2

0.5423666237610907E+04 0.6118691548293858E+07

MEAN VARIANCE VARIANCE OF THE VARIANCES

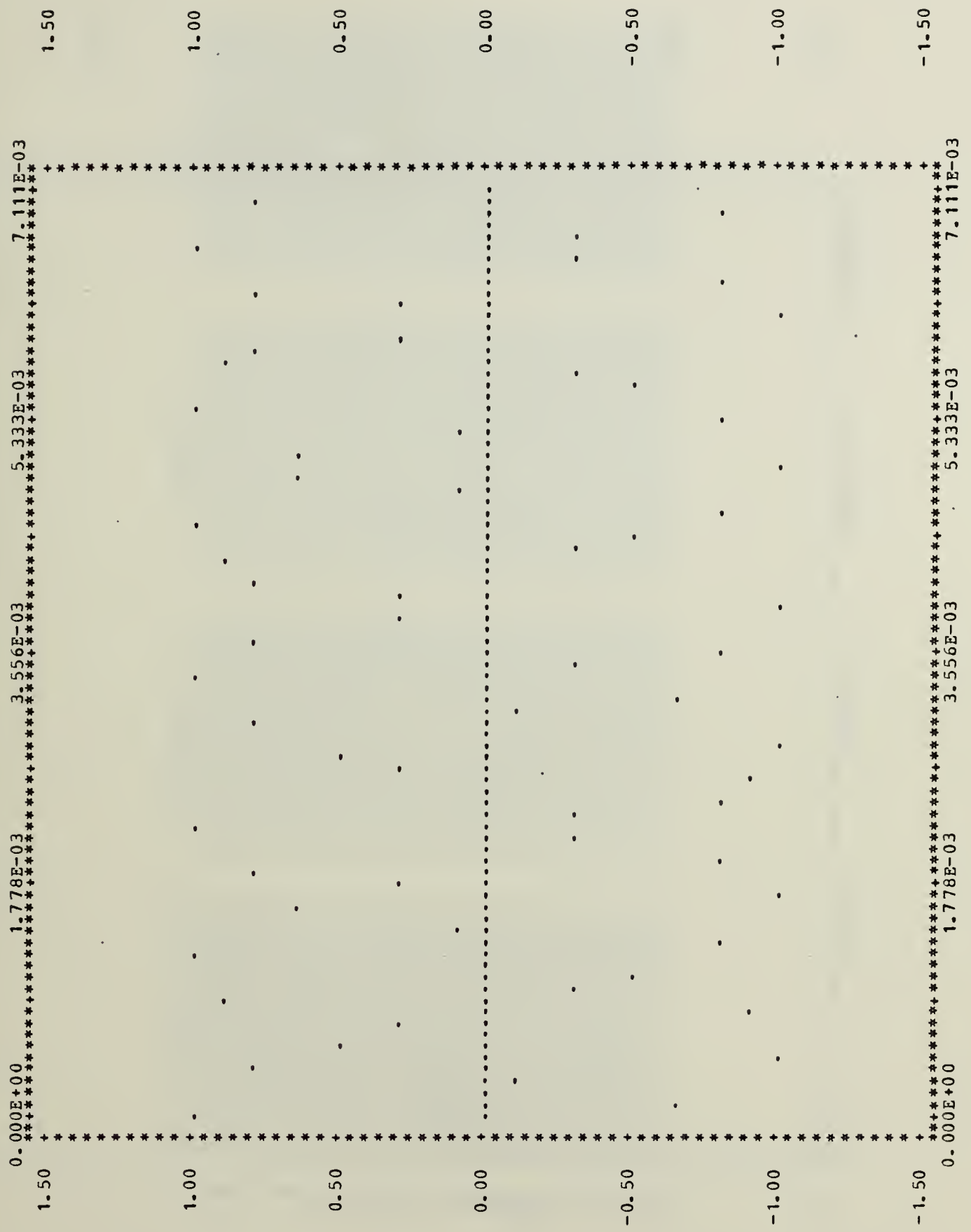
0.4623909548014508E+01 0.4309394443714190E+02

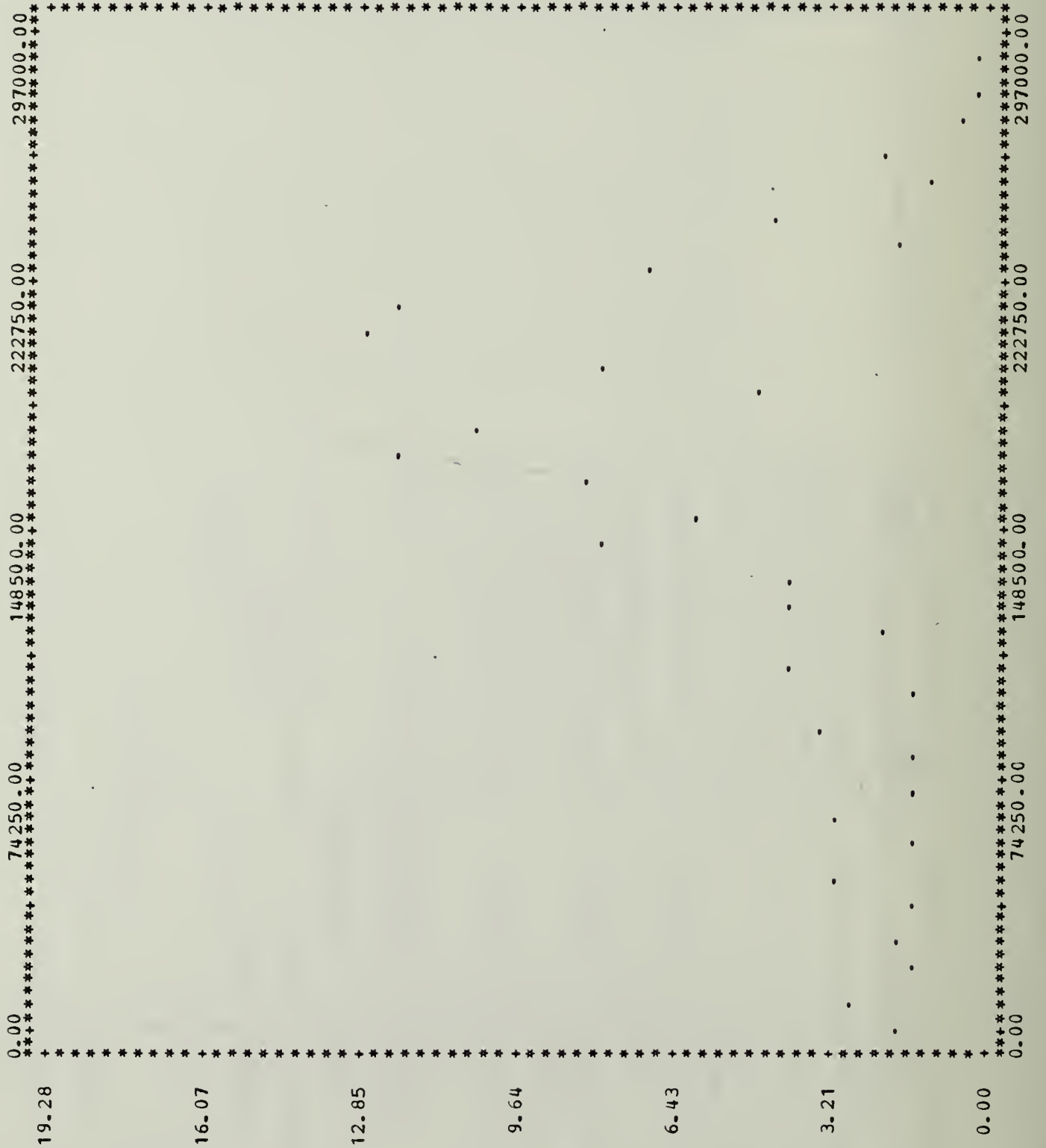
MEAN SKEWNESS VARIANCE OF THE SKEWNESS

-0.5047206845001924E+03 0.2770063131355647E+07

MEAN KURTOSIS VARIANCE OF THE KURTOSIS

0.1643535223518457E+03 0.1633529030650538E+06





N	1	SUM	X**2	SUM	X**2	SUM	X**3	SUM	X**3	SUM	X**4
	2	1745381057261094E+03	4388378241030927E+03	13461104349531155E+04	4708163227179921E+04	0	0	0	0	0	0
	3	1670893117553454E+03	33761733061659528E+03	78445903233160757E+03	2034919190393599E+04	0	0	0	0	0	0
	4	154930198924949759E+03	3011028684335374E+03	7144100088287219E+03	0	0	0	0	0	0	0
	5	16691998924967162E+03	34376884874075052E+03	8167784447618721E+03	0	0	0	0	0	0	0
	6	1793980985469851E+03	38822425787684695E+03	1283686155661075E+04	0	0	0	0	0	0	0
	7	17441980822257994E+03	3874892151236301E+03	9960270919690042E+03	0	0	0	0	0	0	0
	8	2053488485398217E+03	51683838188033192E+03	1367850258262828E+04	0	0	0	0	0	0	0
	9	2088844746733196E+03	52312122606289023E+03	14918355026790559E+04	0	0	0	0	0	0	0
	10	207833508129812E+03	51695323939239922E+03	1500350818620739E+04	0	0	0	0	0	0	0
	11	207833508129812E+03	4500323939239922E+03	1435261336113773E+04	0	0	0	0	0	0	0
	12	184637675184711E+03	622718439669914E+03	1281911761836188E+04	0	0	0	0	0	0	0
	13	224594649482377E+03	11204246335892330E+04	1963667979815342E+04	0	0	0	0	0	0	0
	14	2963675540203763E+03	1251601271582480E+04	4905380513832378E+04	0	0	0	0	0	0	0
	15	3173784304747807E+03	1707980006002793E+04	5689442182858819E+05	0	0	0	0	0	0	0
	16	4614191970595573E+03	261264880821186E+04	114619110245010E+05	0	0	0	0	0	0	0
	17	6056467485580745E+03	4682979409916067E+04	1742546143225242E+05	0	0	0	0	0	0	0
	18	6406800917972383E+03	48787758719176228E+04	4186839325073341E+05	0	0	0	0	0	0	0
	19	1698791308733019E+04	3168438719176228E+04	6324822604024616E+05	0	0	0	0	0	0	0
	20	6683213299026640E+03	5214515827243337E+04	5752818627243337E+04	0	0	0	0	0	0	0
	21	6465666718341274E+04	4910870028871991E+04	4839993126034607E+05	0	0	0	0	0	0	0
	22	454812650914E+04	1460542592979535E+05	4176756170083457E+05	0	0	0	0	0	0	0
	23	1044373719208894E+03	1235549589466912E+05	2141030904177548E+06	0	0	0	0	0	0	0
	24	498105119955246E+03	3119838530726825E+04	1584020909151345E+06	0	0	0	0	0	0	0
	25	4123269596834755E+03	280718963297371694E+03	2260571335915158E+06	0	0	0	0	0	0	0
	26	2864935711027876E+03	4147963297371694E+03	1304784189728246E+05	0	0	0	0	0	0	0
	27	1801795405150350E+03	2085390938171418E+03	3770017149804132E+04	0	0	0	0	0	0	0
	28	1309968810623288E+03	9649084057365933E+02	3929666456011763E+04	0	0	0	0	0	0	0
	29	8612683898396291E+02	4436495121812613E+02	7929666456011763E+04	0	0	0	0	0	0	0
	30	6043016238925039E+02	371233360301779964E+02	36010705618402255E+03	0	0	0	0	0	0	0
	31	5680265238925039E+02	4371233360301779964E+02	26258834219462338E+02	0	0	0	0	0	0	0
	32										
	33										

MODULATION TECHNIQUE = MFSK

BIFOLAR LOGIC

BAUD OR SYMBOL RATE = 1200 HZ

BITS PER BINARY CODE WORD = 3

BIT RATE = 0.3600000000000000E+04

CARRIER FREQUENCY = 10800 HZ

MAXIMUM CARRIER AMPLITUDE = 1 VOLT(S)

INITIAL PHASE ANGLE = 0 DEGREES

TIME BETWEEN SAMPLES = 0.3086419753086419E-04 SEC

NUMBER OF SAMPLES GENERATED = 64

SEED FOR RANDOM NUMBER GENERATOR = 1

NUMBER OF TIMES SIMULATION REPEATS = 100

SUM OF VARIANCES SUM OF VARIANCES**2

0.4806181141925261E+03 0.1352273679574422E+05

SUM OF SKEWNESS SUM OF SKEWNESS**2

-0.1654247621695240E+04 0.5890267815807785E+06

SUM OF KURTOSIS SUM OF KURTOSIS**2

0.5341287673934422E+05 0.2790612658473240E+09

MEAN VARIANCE VARIANCE OF THE VARIANCES

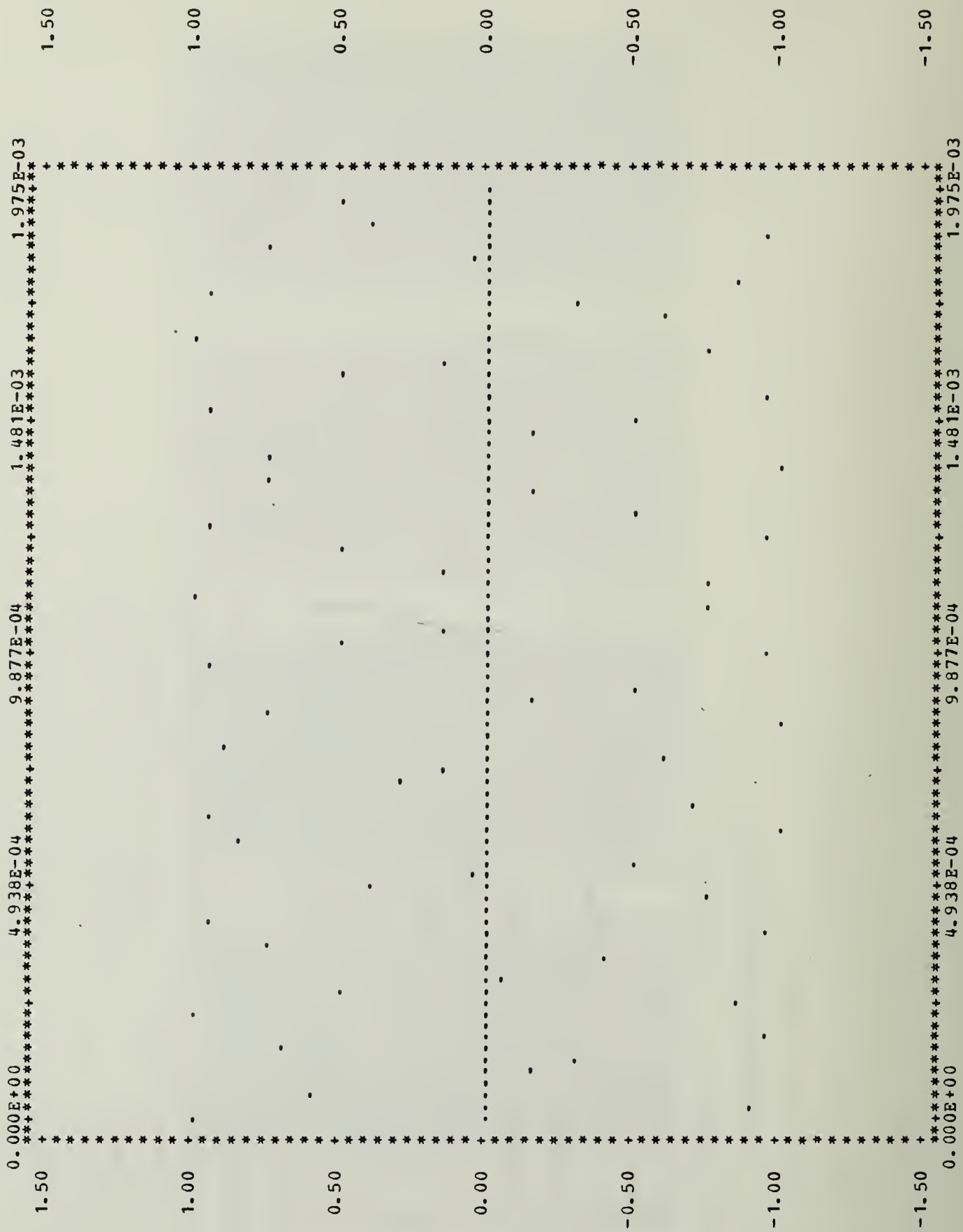
0.1456418527856140E+02 0.2038414228878589E+03

MEAN SKEWNESS VARIANCE OF THE SKEWNESS

-0.5012871580894667E+02 0.1581567102109974E+05

MEAN KURTOSIS VARIANCE OF THE KURTOSIS

0.1618572022404370E+04 0.6019021185027759E+07

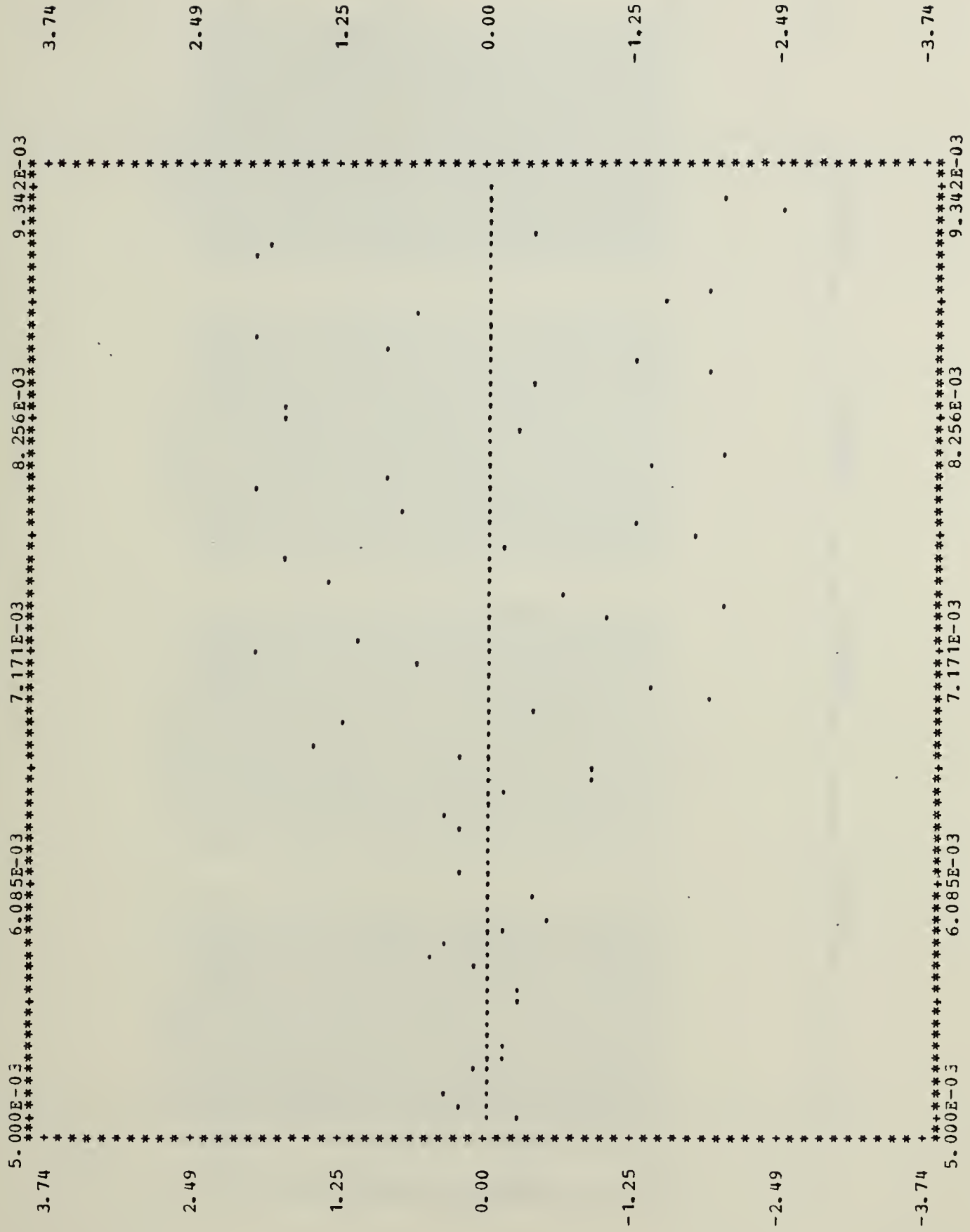




N	MEAN	VARIANCE	SKENNESS	KURTOSIS
1	24212703	1701870281944493E+00	812215818899301E+00	5202216579936257E-01
2	2119943275051E+00	1692179389704175E+00	1870091187221E+00	4962377142977347E-01
3	1560497944E+00	1630844574986009E+00	29752098096693356E+00	475992390494947E-01
4	602695775089775E+00	1517438865402408E+00	030112971176993356E+00	40605584454262756E-01
5	6003884574738126E+00	15413102275696224E+00	322279329193875E+00	5372574080699803E-01
6	691491147335869E+00	1625277259407340E+00	33037301580382245E+00	6338732183899803E-01
7	712915135223571E+00	19894592044684256E+00	345738416523099339E+00	9079440007191118E-01
8	83470574018743954E+00	21585339047272559E+00	2513665218179688E+00	8711759471530689E-01
9	11552036641180799E+01	3253381023466752E+00	162587555816594E+00	7897411259783627E-01
10	140557865404239E+01	5901481998178570E+00	361671703060194E+00	3009444434532169E+00
11	1653469595833664E+01	10064089090697685E+01	1545347282296657E+01	6485308087822852E+00
12	22094270411689E+01	860465303472624543E+01	27645225934540579E+01	1839454693919151E+01
13	53027928805043730E+01	44993844561945615E+02	1192554149182590E+02	1742698305978736E+03
14	5652678805043730E+01	311622837110405E+02	19150663623557811E+03	8114244563340110E+03
15	48392266056893745E+01	1627827150809915E+02	1153475974583148E+03	5030156057294299E+04
16	47999226056893745E+01	660039482645575E+02	1210599846314087E+03	102701519590084E+04
17	4949076398807320E+01	3195721379055708E+02	1586666023965808E+03	9267637549136898E+04
18	4949076398807320E+01	17108619009518350E+02	129447224886342935E+03	6953906279136898E+04
19	567650996298115E+01	4183417025969290E+02	1323276886342935E+03	151876067790119E+04
20	6101993577152731E+01	167702074722844268E+02	2215862356984157E+03	79327409866113413E+03
21	6259114577537281E+01	262812246433581870E+02	2779436555304021E+03	1949698968797135E+04
22	62844277487325188E+01	128212246433581870E+02	2785797147037739E+03	2129199108385613E+04
23	5170868203869401E+01	2976675343581870E+02	3721000245806551E+02	4954058112039018E+03
24	5917383281247872E+01	14966293222255E+02	521211021481788E+02	2486653252310702E+04
25	54103076669056E+01	3540159338958492E+02	26041244531555488E+02	1728196939758512E+04
26	52887454282284268E+01	1787438121393946E+02	202894659598615E+02	4059766140333669E+04
27	5074754282284268E+01	3131561713839394E+02	202894659598615E+02	6603169983834629E+04
28	4253074282284268E+01	577288744924743E+01	1173219615183384E+01	290590500634774E+04
29	19337545429384470E+01	2626549296496931E+01	3205281031167369E+01	2345083299105233E+02
30	1137815044472511E+01	1207462920504103E+01	1860809816827437E+01	2094124943883444E+02
31				71689252358522774E+01
32				
33				

N	Y	SUM	X**2	X**3	X**4
1	2703	2421	7209	19683	531441
2	1994	1994	3976	7928	158424
3	1560	1560	2430	3808	59049
4	977	977	954	938	91437
5	884	884	781	688	60523
6	775	775	600	463	35937
7	735	735	540	398	29247
8	735	735	540	398	29247
9	1291	1291	1666	2167	282429
10	743	743	552	408	30270
11	2036	2036	8145	16688	341472
12	365	365	133	49	1770
13	404	404	163	66	2688
14	583	583	340	233	13122
15	504	504	254	128	6496
16	298	298	88	25	2144
17	554	554	307	170	10850
18	411	411	169	57	2494
19	366	366	134	39	1382
20	569	569	324	186	10648
21	1051	1051	1104	1155	12167
22	996	996	992	986	98608
23	774	774	599	463	35937
24	577	577	333	200	1372
25	1145	1145	1309	1513	19683
26	277	277	76	20	1385
27	487	487	238	116	3383
28	382	382	146	53	779
29	124	124	15	2	220
30	766	766	587	450	34640
31	333	333	111	39	1369
32	422	422	178	75	3152
33	150	150	22	3	337

MODULATION TECHNIQUE = QPRS
 QPFS CLASS 1 FILTER
 BIFOLAR LOGIC
 BAUD OR SYMBOL RATE = 1200 HZ
 BITS PER BINARY CODE WORD = 2
 BIT RATE = 0.2400000000000000E+04
 CARRIER FREQUENCY = 2400 HZ
 MAXIMUM CARRIER AMPLITUDE = 1 VOLT(S)
 INITIAL PHASE ANGLE = 0 DEGREES
 TIME BETWEEN SAMPLES = 0.6784342273548912E-04 SEC
 NUMBER OF SAMPLES GENERATED = 64
 SEED FOR RANDOM NUMBER GENERATOR = 1
 NUMBER OF TIMES SIMULATION REPEATS = 100
 SUM OF VARIANCES SUM OF VARIANCES**2
 0.7925891201989905E+03 0.1512135267846902E+06
 SUM OF SKEWNESS SUM OF SKEWNESS**2
 -0.1732359062524069E+06 0.9850778236273860E+10
 SUM OF KURTOSIS SUM OF KURTOSIS**2
 0.3533192079165041E+06 0.4536060891356758E+11
 MEAN VARIANCE VARIANCE OF THE VARIANCES
 0.2401785212724214E+02 0.4130538703065308E+04
 MEAN SKEWNESS VARIANCE OF THE SKEWNESS
 -0.5249572916739602E+04 0.2794176160813870E+09
 MEAN KURTOSIS VARIANCE OF THE KURTOSIS
 0.1070664266413649E+05 0.1299304575250932E+10



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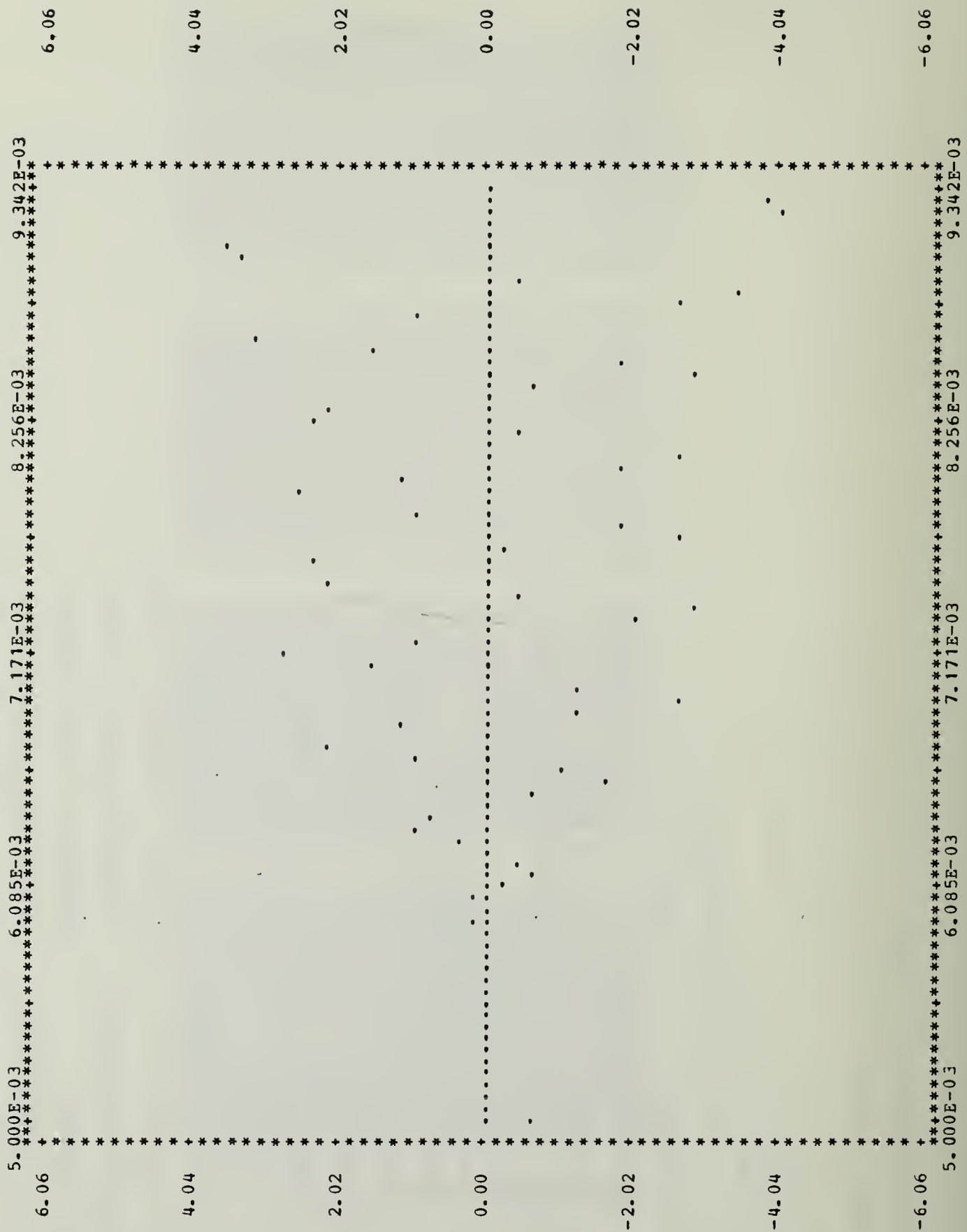
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+ * * * * *
57.04
+ * * * * *
47.54
+ * * * * *
38.03
+ * * * * *
28.52
+ * * * * *
19.01
+ * * * * *
9.51
+ * * * * *
0.00
+ * * * * *
0.00 ***** 121603.62 ***** 243207.12 ***** 364810.62 ***** 486414.12 *****
+ * * * * *

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N	MEAN	VARIANCE	SKENBRS	KURTOSIS
1	1746.8113	1388348922	22827702	51409226308007252E+01
2	1783.9340	1373900559	22838369571580200E+01	0-50760960436444750E+01
3	1881.6395	13911537145	19635911680200E+01	0-5267763272060726E+01
4	2047.6865	1468678508	1745328097E+01	0-5884490676168223E+01
5	2297.3885	1644047473	17535370515E+02	0-7239435166189224E+01
6	2683.5056	1999006627	1823186803260518E+02	0-1024292414275401E+02
7	3312.9241	2756479367	176250788E+02	0-1834851180285642E+02
8	3536.5525	4811195957	168023396E+03	0-5414450274312225E+02
9	3232.8564	1129481209	196860526031E+04	0-140913763345369462E+02
10	3232.8564	2402926487	155013949577E+05	0-27353204731804624E+05
11	3232.8564	2623380860	159761041918E+05	0-1283904745345857E+06
12	2012.3686	404390696	429734775E+05	0-1648935745345857E+06
13	2150.2438	1051549869	469756025E+05	0-27353204731804624E+05
14	2016.3485	1396152524	48149481494E+03	0-4730046115964915E+03
15	2970.0807	4194625326	451504106E+02	0-4603296277462294E+02
16	2390.8749	2376936951	49528176027253E+02	0-77635857737947988E+01
17	2016.8125	1211509773	4481281848517E+01	0-46299456838253585E+01
18	1753.5741	9704493989	49409356771873E+01	0-31144408386156138E+01
19	1558.9355	814815824	528335216646E+00	0-2271002271430383E+01
20	1408.7366	7084187569	304352912087E+01	0-17547462256637649E+01
21	1290.8263	632716575	25878660303746E+00	0-1417160155580148E+01
22	1196.2766	577355748	20678660303746E+00	0-1185743805976271E+01
23	1119.6272	4361642063	339356593949C9E-01	0-9026889684670851E+00
24	1056.5671	4821300846	3337377691836187E+00	0-8152494762041542E+00
25	1004.8541	4650482001	3337377691836187E+00	0-703802974033507E+00
26	927.3989	4528007126	3337377691836187E+00	0-67045456753391549E+00
27	862.9671	4445214050	3337377691836187E+00	0-6481934210539040E+00
28	800.1157	4395214050	3337377691836187E+00	0-6351869105735284E+00
29	788.2088	4372540540	3337377691836187E+00	0-6299589957549781E+00
30	862.9671	4371419567	3337377691836187E+00	0-6304885575454902E+00
31	852.9998	4382132490	3337377691836187E+00	0-6304885575454902E+00
32	849.0527	4382132490	3337377691836187E+00	0-6304885575454902E+00
33	849.0527	4382132490	3337377691836187E+00	0-6304885575454902E+00

N	X	Y	SUM	X**2	Y**2	X*Y	SUM	X**3	Y**3	X*Y	SUM	X**4	Y**4	X*Y	SUM
1	1746	8113	14185	3038	6581	11385	13488	1746	5181	13488	13488	4629	1746	13488	4629
2	1783	9340	16627	3180	8712	15480	15882	1783	6850	15480	15882	4822	1783	15882	4822
3	1845	6867	12712	3383	4714	12611	12611	1845	6142	12611	12611	5476	1845	12611	5476
4	2297	3885	8841	5205	1508	10542	10542	2297	5205	10542	10542	6851	2297	10542	6851
5	2683	5054	13465	7199	2554	17002	17002	2683	5054	17002	17002	9659	2683	17002	9659
6	3312	9241	21201	10970	8539	36801	36801	3312	11516	36801	36801	1597	3312	36801	1597
7	4514	7555	33869	20322	5706	103218	103218	4514	8126	103218	103218	3353	4514	103218	3353
8	9536	5514	52850	90904	3040	52850	52850	9536	3040	52850	52850	1095	9536	52850	1095
9	2195	5557	12112	4818	3088	12112	12112	2195	3088	12112	12112	2406	2195	12112	2406
10	3232	8564	27548	10448	7314	27548	27548	3232	7314	27548	27548	2406	3232	27548	2406
11	3529	6640	23444	12456	4408	23444	23444	3529	4408	23444	23444	6097	3529	23444	6097
12	2012	3686	7444	4048	1357	7444	7444	2012	1357	7444	7444	2406	2012	7444	2406
13	7502	3686	27548	5628	1357	27548	27548	7502	1357	27548	27548	8978	7502	27548	8978
14	4016	3488	13864	1613	1200	13864	13864	4016	1200	13864	13864	2406	4016	13864	2406
15	2970	9807	29227	8821	9614	29227	29227	2970	9614	29227	29227	8821	2970	29227	8821
16	2390	8746	20936	5713	7648	20936	20936	2390	7648	20936	20936	5713	2390	20936	5713
17	2016	8122	16304	4064	6600	16304	16304	2016	6600	16304	16304	8122	2016	16304	8122
18	1558	7357	11355	2427	5407	11355	11355	1558	5407	11355	11355	2427	1558	11355	2427
19	1408	7357	10355	1982	5407	10355	10355	1408	5407	10355	10355	2427	1408	10355	2427
20	1290	8266	10656	1681	6825	10656	10656	1290	6825	10656	10656	1681	1290	10656	1681
21	1196	2726	3268	1428	7441	3268	3268	1196	7441	3268	3268	1428	1196	3268	1428
22	1056	5671	5985	1115	3214	5985	5985	1056	3214	5985	5985	1115	1056	5985	1115
23	1004	8541	8541	1008	7288	8541	8541	1004	7288	8541	8541	1008	1004	8541	1008
24	9623	9894	9894	9259	9778	9894	9894	9623	9778	9894	9894	9259	9623	9894	9259
25	9278	1277	11505	8600	1622	11505	11505	9278	1622	11505	11505	8600	9278	11505	8600
26	9001	1157	10428	8123	1322	10428	10428	9001	1322	10428	10428	8123	9001	10428	8123
27	8786	2888	11674	7648	8155	11674	11674	8786	8155	11674	11674	7648	8786	11674	7648
28	8529	9980	18509	7255	9960	18509	18509	8529	9960	18509	18509	7255	8529	18509	7255
29	8490	5215	13705	7200	2705	13705	13705	8490	2705	13705	13705	7200	8490	13705	7200
30	8490	5215	13705	7200	2705	13705	13705	8490	2705	13705	13705	7200	8490	13705	7200
31	8490	5215	13705	7200	2705	13705	13705	8490	2705	13705	13705	7200	8490	13705	7200
32	8490	5215	13705	7200	2705	13705	13705	8490	2705	13705	13705	7200	8490	13705	7200
33	8490	5215	13705	7200	2705	13705	13705	8490	2705	13705	13705	7200	8490	13705	7200

MODULATION TECHNIQUE = QPRS
 QPRS CLASS 2 FILTER
 BIFOLAR LOGIC
 BAUD OR SYMBOL RATE = 1200 HZ
 BITS PER BINARY CODE WORD = 2
 BIT RATE = 0.2400000000000000E+04
 CARRIER FREQUENCY = 2400 HZ
 MAXIMUM CARRIER AMPLITUDE = 1 VOLT(S)
 INITIAL PHASE ANGLE = 0 DEGREES
 TIME BETWEEN SAMPLES = 0.6784342273548912E-04 SEC
 NUMBER OF SAMPLES GENERATED = 64
 SEED FOR RANDOM NUMBER GENERATOR = 1
 NUMBER OF TIMES SIMULATION REPEATS = 100
 SUM OF VARIANCES SUM OF VARIANCES**2
 0.2406301297164022E+04 0.1712404031156036E+07
 SUM OF SKEWNESS SUM OF SKEWNESS**2
 -0.1014071770004887E+07 0.4097280851254902E+12
 SUM OF KURTOSIS SUM OF KURTOSIS**2
 0.4062278349001294E+07 0.7316406994491162E+13
 MEAN VARIANCE VARIANCE OF THE VARIANCES
 0.7291822112618248E+02 0.4802940065853782E+05
 MEAN SKEWNESS VARIANCE OF THE SKEWNESS
 -0.3072944757590566E+05 0.1183019436971622E+11
 MEAN KURTOSIS VARIANCE OF THE KURTOSIS
 0.1230993439091301E+06 0.2130107248422762E+12

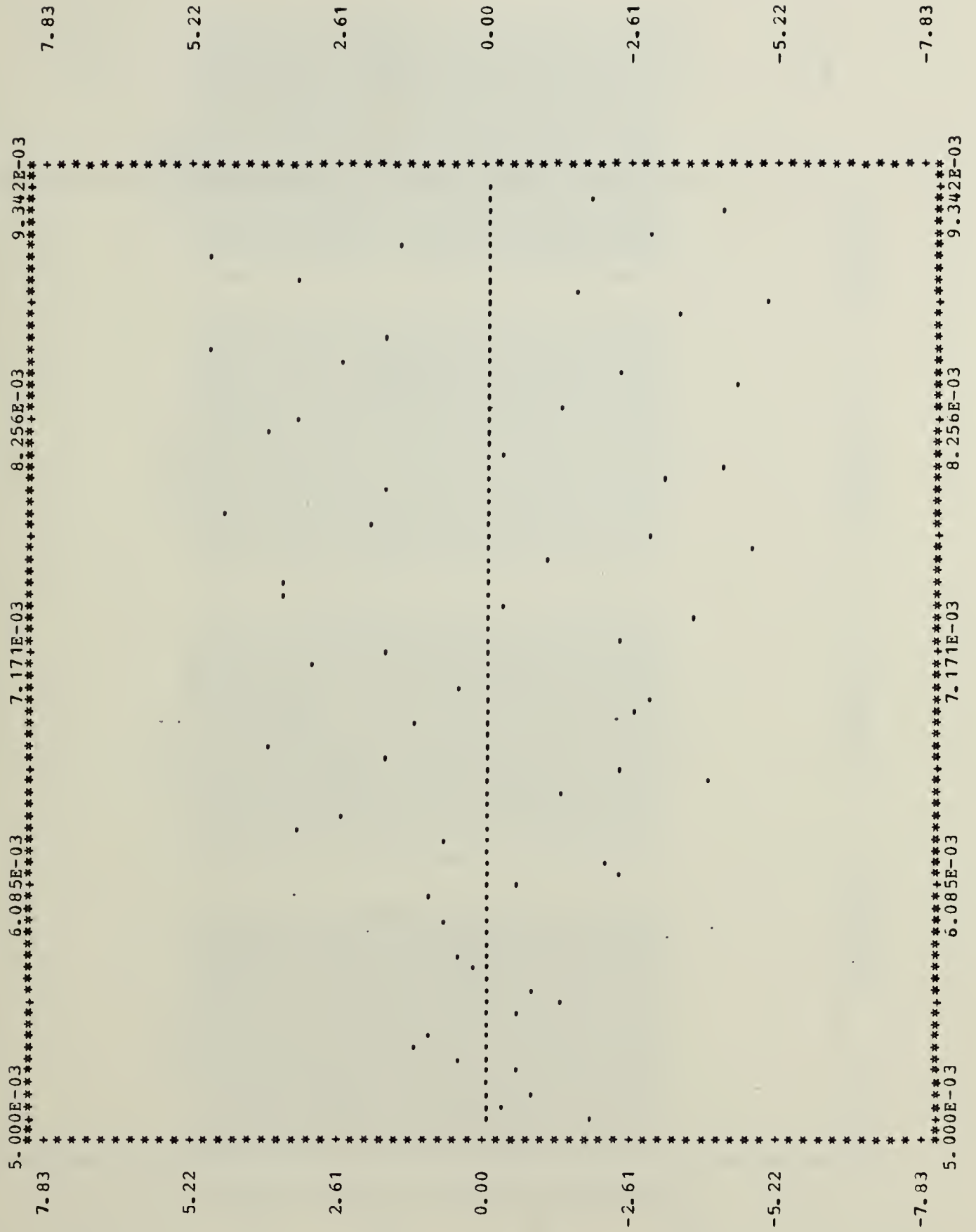


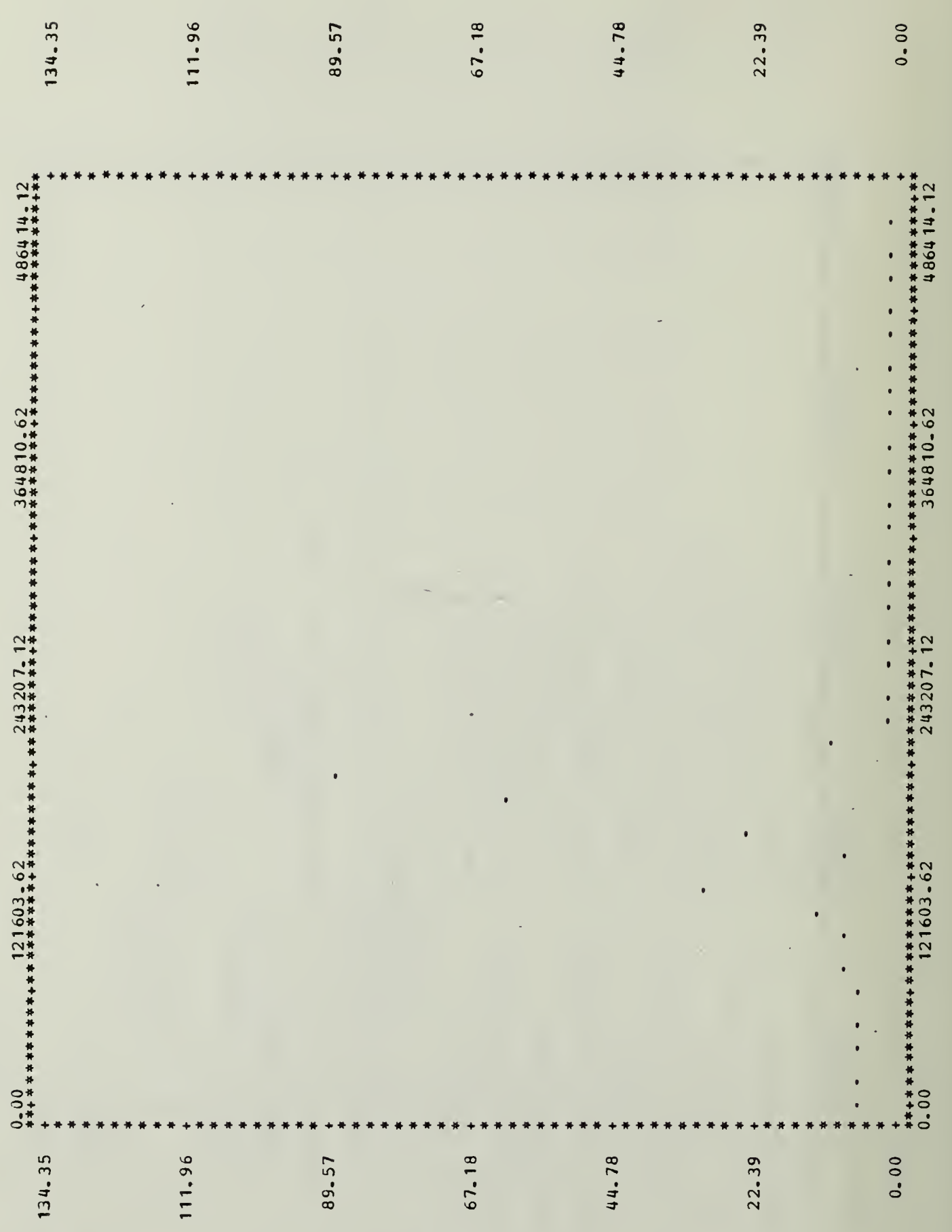


N	MEAN	VARIANCE	SKWENESS	KURTOSIS
1	288374	3992201	-0.25	0.4693
2	42776	201408	-0.27	1.1752
3	575697	305201	-0.34	1.1439
4	787561	664962	-0.48	1.9143
5	330994	1239933	-0.74	1.2063
6	304769	2889193	-0.74	1.2063
7	464961	296521	-0.12	0.8996
8	496188	1503510	-0.23	1.1651
9	1829987	1891019	-0.36	1.5165
10	265467	688704	-0.26	1.1855
11	246406	139704	-0.15	0.5682
12	152818	818768	-0.21	1.1855
13	251528	337355	-0.43	1.2194
14	276503	237352	-0.41	1.1050
15	124242	376952	-0.18	0.4049
16	396408	255801	-0.22	0.5478
17	543300	143811	-0.50	1.2054
18	275091	158549	-0.39	1.4298
19	157695	769524	-0.37	1.4825
20	726489	396073	-0.22	0.6900
21	303167	113118	-0.19	0.1082
22	203033	167113	-0.25	0.5150
23	177464	770187	-0.10	0.0826
24	989967	659938	-0.21	0.5751
25	1349906	892020	-0.20	0.1844
26	1816480	2072585	-0.39	1.1978
27	579447	958521	-0.39	1.1978
28	580662	637884	-0.34	0.9948
29	715922	405270	-0.52	1.3799
30	162433	224057	-0.51	1.4851
31	155164	579334	-0.51	1.2269
32	160566	338543	-0.51	1.3800
33	164814	566385	-0.12	0.7668
34	164814	566385	-0.12	0.7668
35	164814	566385	-0.12	0.7668
36	164814	566385	-0.12	0.7668
37	164814	566385	-0.12	0.7668
38	164814	566385	-0.12	0.7668
39	164814	566385	-0.12	0.7668
40	164814	566385	-0.12	0.7668
41	164814	566385	-0.12	0.7668
42	164814	566385	-0.12	0.7668
43	164814	566385	-0.12	0.7668
44	164814	566385	-0.12	0.7668
45	164814	566385	-0.12	0.7668
46	164814	566385	-0.12	0.7668
47	164814	566385	-0.12	0.7668
48	164814	566385	-0.12	0.7668
49	164814	566385	-0.12	0.7668
50	164814	566385	-0.12	0.7668
51	164814	566385	-0.12	0.7668
52	164814	566385	-0.12	0.7668
53	164814	566385	-0.12	0.7668
54	164814	566385	-0.12	0.7668
55	164814	566385	-0.12	0.7668
56	164814	566385	-0.12	0.7668
57	164814	566385	-0.12	0.7668
58	164814	566385	-0.12	0.7668
59	164814	566385	-0.12	0.7668
60	164814	566385	-0.12	0.7668
61	164814	566385	-0.12	0.7668
62	164814	566385	-0.12	0.7668
63	164814	566385	-0.12	0.7668
64	164814	566385	-0.12	0.7668
65	164814	566385	-0.12	0.7668
66	164814	566385	-0.12	0.7668
67	164814	566385	-0.12	0.7668
68	164814	566385	-0.12	0.7668
69	164814	566385	-0.12	0.7668
70	164814	566385	-0.12	0.7668
71	164814	566385	-0.12	0.7668
72	164814	566385	-0.12	0.7668
73	164814	566385	-0.12	0.7668
74	164814	566385	-0.12	0.7668
75	164814	566385	-0.12	0.7668
76	164814	566385	-0.12	0.7668
77	164814	566385	-0.12	0.7668
78	164814	566385	-0.12	0.7668
79	164814	566385	-0.12	0.7668
80	164814	566385	-0.12	0.7668
81	164814	566385	-0.12	0.7668
82	164814	566385	-0.12	0.7668
83	164814	566385	-0.12	0.7668
84	164814	566385	-0.12	0.7668
85	164814	566385	-0.12	0.7668
86	164814	566385	-0.12	0.7668
87	164814	566385	-0.12	0.7668
88	164814	566385	-0.12	0.7668
89	164814	566385	-0.12	0.7668
90	164814	566385	-0.12	0.7668
91	164814	566385	-0.12	0.7668
92	164814	566385	-0.12	0.7668
93	164814	566385	-0.12	0.7668
94	164814	566385	-0.12	0.7668
95	164814	566385	-0.12	0.7668
96	164814	566385	-0.12	0.7668
97	164814	566385	-0.12	0.7668
98	164814	566385	-0.12	0.7668
99	164814	566385	-0.12	0.7668
100	164814	566385	-0.12	0.7668

N	X	SUM	X**2	X**3	SUM	X**3	SUM	X**4
1	2883	7442	8226	5277	1784	2708	5205	1457
2	2945	7556	9837	6768	2508	1498	5985	1792
3	3112	7787	11568	7758	3642	2508	6223	1983
4	3392	8056	13695	9185	5866	3934	8522	2361
5	3814	8309	15260	10953	8273	5446	11389	2955
6	4448	8347	16994	12550	11616	7334	15838	3904
7	4446	8496	17399	13094	11613	7322	15835	3902
8	4721	8587	18199	13662	11615	7324	15837	3903
9	5274	8654	18867	14229	11617	7326	15839	3905
10	6158	8704	19406	14800	11619	7328	15841	3907
11	6100	8715	19428	14811	11620	7329	15842	3908
12	6100	8715	19428	14811	11620	7329	15842	3908
13	6100	8715	19428	14811	11620	7329	15842	3908
14	6100	8715	19428	14811	11620	7329	15842	3908
15	6100	8715	19428	14811	11620	7329	15842	3908
16	6100	8715	19428	14811	11620	7329	15842	3908
17	6100	8715	19428	14811	11620	7329	15842	3908
18	6100	8715	19428	14811	11620	7329	15842	3908
19	6100	8715	19428	14811	11620	7329	15842	3908
20	6100	8715	19428	14811	11620	7329	15842	3908
21	6100	8715	19428	14811	11620	7329	15842	3908
22	6100	8715	19428	14811	11620	7329	15842	3908
23	6100	8715	19428	14811	11620	7329	15842	3908
24	6100	8715	19428	14811	11620	7329	15842	3908
25	6100	8715	19428	14811	11620	7329	15842	3908
26	6100	8715	19428	14811	11620	7329	15842	3908
27	6100	8715	19428	14811	11620	7329	15842	3908
28	6100	8715	19428	14811	11620	7329	15842	3908
29	6100	8715	19428	14811	11620	7329	15842	3908
30	6100	8715	19428	14811	11620	7329	15842	3908
31	6100	8715	19428	14811	11620	7329	15842	3908
32	6100	8715	19428	14811	11620	7329	15842	3908
33	6100	8715	19428	14811	11620	7329	15842	3908

MODULATION TECHNIQUE = QPRS
 QPRS CLASS 3 FILTER
 BIFOLAR LOGIC
 BAUD OR SYMBOL RATE = 1200 HZ
 BITS PER BINARY CODE WORD = 2
 BIT RATE = 0.2400000000000000E+04
 CARRIER FREQUENCY = 2400 HZ
 MAXIMUM CARRIER AMPLITUDE = 1 VOLT(S)
 INITIAL PHASE ANGLE = 0 DEGREES
 TIME BETWEEN SAMPLES = 0.6784342273548912E-04 SEC
 NUMBER OF SAMPLES GENERATED = 64
 SEED FOR RANDOM NUMBER GENERATOR = 1
 NUMBER OF TIMES SIMULATION REPEATS = 100
 SUM OF VARIANCES SUM OF VARIANCES**2
 0.2212313780321216E+04 0.9349388767869366E+06
 SUM OF SKEWNESS SUM OF SKEWNESS**2
 -0.7876831322230185E+06 0.1444178694786092E+12
 SUM OF KURTOSIS SUM OF KURTOSIS**2
 0.2375351460755018E+07 0.1504008831530188E+13
 MEAN VARIANCE VARIANCE OF THE VARIANCES
 0.6703981152488534E+02 0.2458205556000923E+05
 MEAN SKEWNESS VARIANCE OF THE SKEWNESS
 -0.2386918582493996E+05 0.3925516075762725E+10
 MEAN KURTOSIS VARIANCE OF THE KURTOSIS
 0.7198034729560660E+05 0.4165719401362236E+11



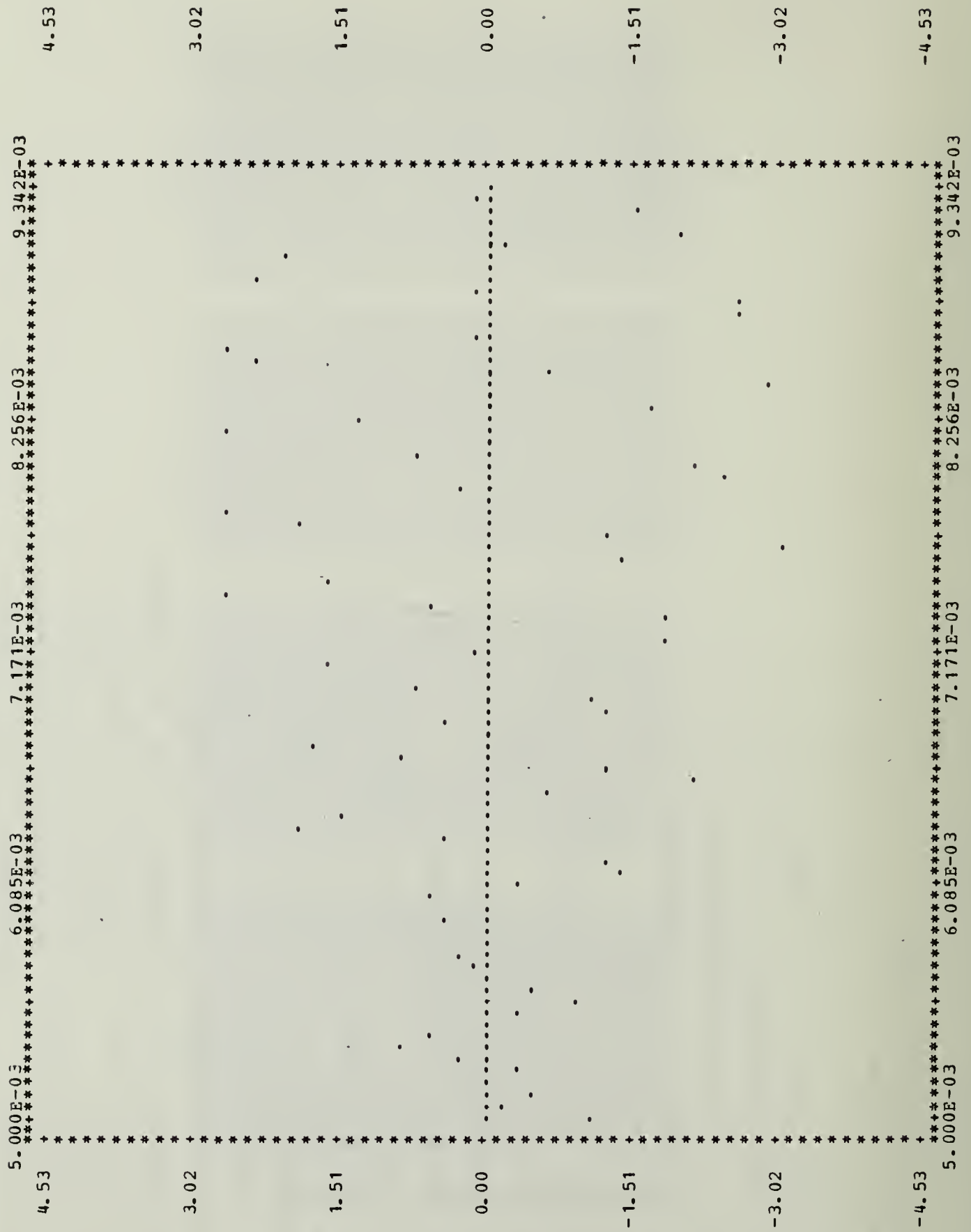


0.00 134.35 111.96 89.57 67.18 44.78 22.39 0.00

0.00 134.35 111.96 89.57 67.18 44.78 22.39 0.00

N	MEAN	VARIANCE	SKENNESS	KURTOSIS
1	2859	4053	8872	5158
2	2941	3960	8255	5214
3	3472	3965	2989	5353
4	3969	4860	0017	6225
5	4735	6300	9437	8273
6	6018	9364	1494	1321
7	8654	2089	2701	2903
8	2281	4339	1776	1229
9	4754	3933	3955	5033
10	4244	4648	2774	4063
11	4636	5580	2234	4793
12	5717	7836	4691	9229
13	4966	4552	0084	4063
14	4540	5858	0234	4793
15	8010	1596	7652	6131
16	5748	7781	1913	1547
17	5873	4291	4494	1220
18	3356	3458	1854	1852
19	2700	1947	2853	1288
20	2893	1617	7844	9657
21	2887	1335	6030	6375
22	4361	1297	4193	5226
23	5702	1065	2096	3022
24	6034	1031	1531	5085
25	5702	1020	2348	5912
26	4821	1045	3201	4653
27	7847	1073	3906	4474
28	3997	1107	3322	4543
29	4887	1143	3084	4811
30	7948	1107	3322	4543
31	4857	1107	3322	4543
32	4742	1165	8592	4923
33	4895	1165	8592	4923

MODULATION TECHNIQUE = QPRS
 QPRS CLASS 4 FILTER
 BIFOLAR LOGIC
 BAUD OR SYMBOL RATE = 1200 HZ
 BITS PER BINARY CODE WORD = 2
 BIT RATE = 0.2400000000000000E+04
 CARRIER FREQUENCY = 2400 HZ
 MAXIMUM CARRIER AMPLITUDE = 1 VOLT (S)
 INITIAL PHASE ANGLE = 0 DEGREES
 TIME BETWEEN SAMPLES = 0.6784342273548912E-04 SEC
 NUMBER OF SAMPLES GENERATED = 64
 SEED FOR RANDOM NUMBER GENERATOR = 1
 NUMBER OF TIMES SIMULATION REPEATS = 100
 SUM OF VARIANCES. SUM OF VARIANCES**2
 0.7516311188359808E+03 0.1147433777377834E+06
 SUM OF SKEWNESS SUM OF SKEWNESS**2
 -0.1502958760239533E+06 0.5926297375617011E+10
 SUM OF KURTOSIS SUM OF KURTOSIS**2
 0.3178921864476514E+06 0.3285296126177793E+11
 MEAN VARIANCE VARIANCE OF THE VARIANCES
 0.2277670057078729E+02 0.3050740650136574E+04
 MEAN SKEWNESS VARIANCE OF THE SKEWNESS
 -0.4554420485574342E+04 0.1638058362173805E+09
 MEAN KURTOSIS VARIANCE OF THE KURTOSIS
 0.9633096559019739E+04 0.9309585979490561E+09

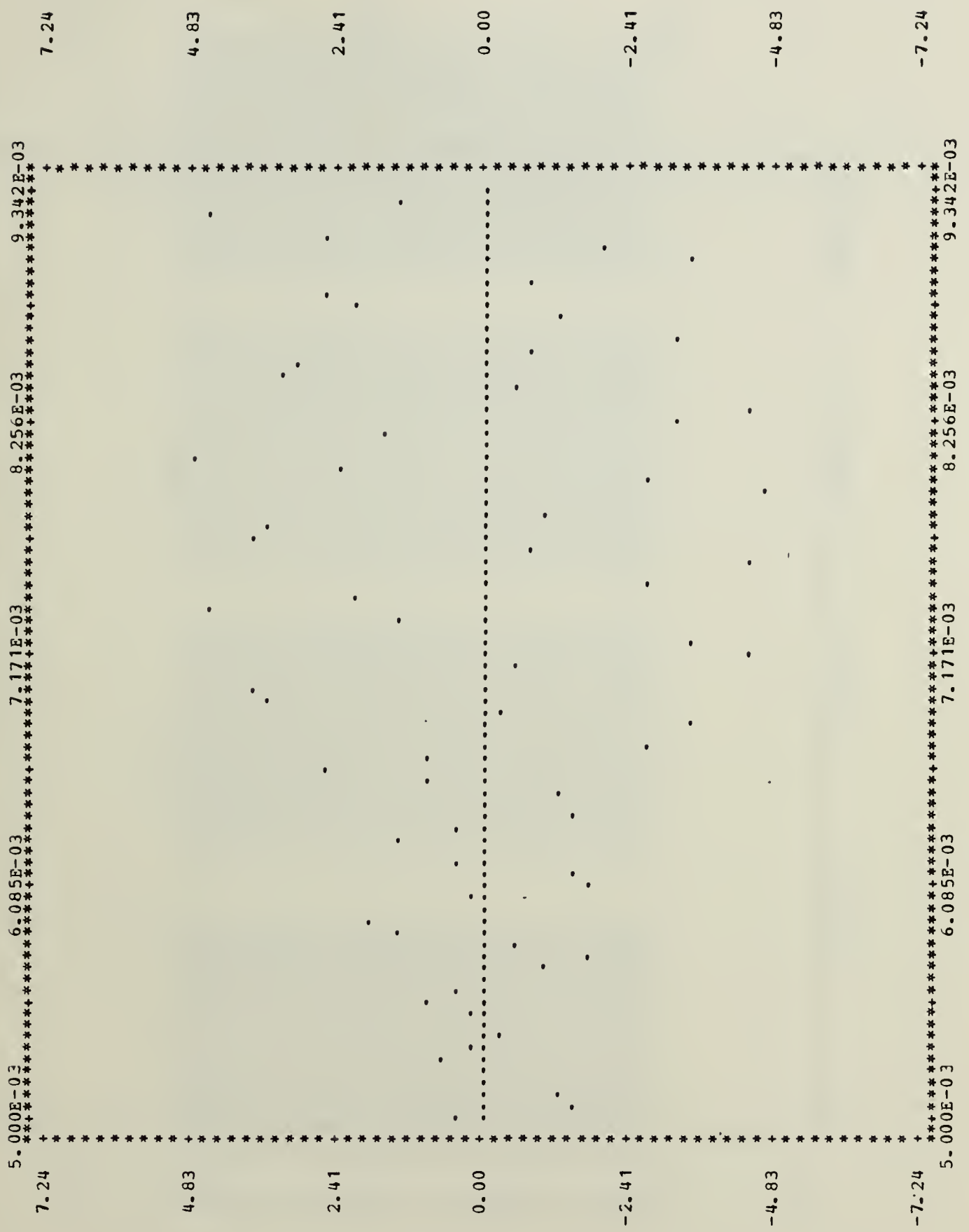


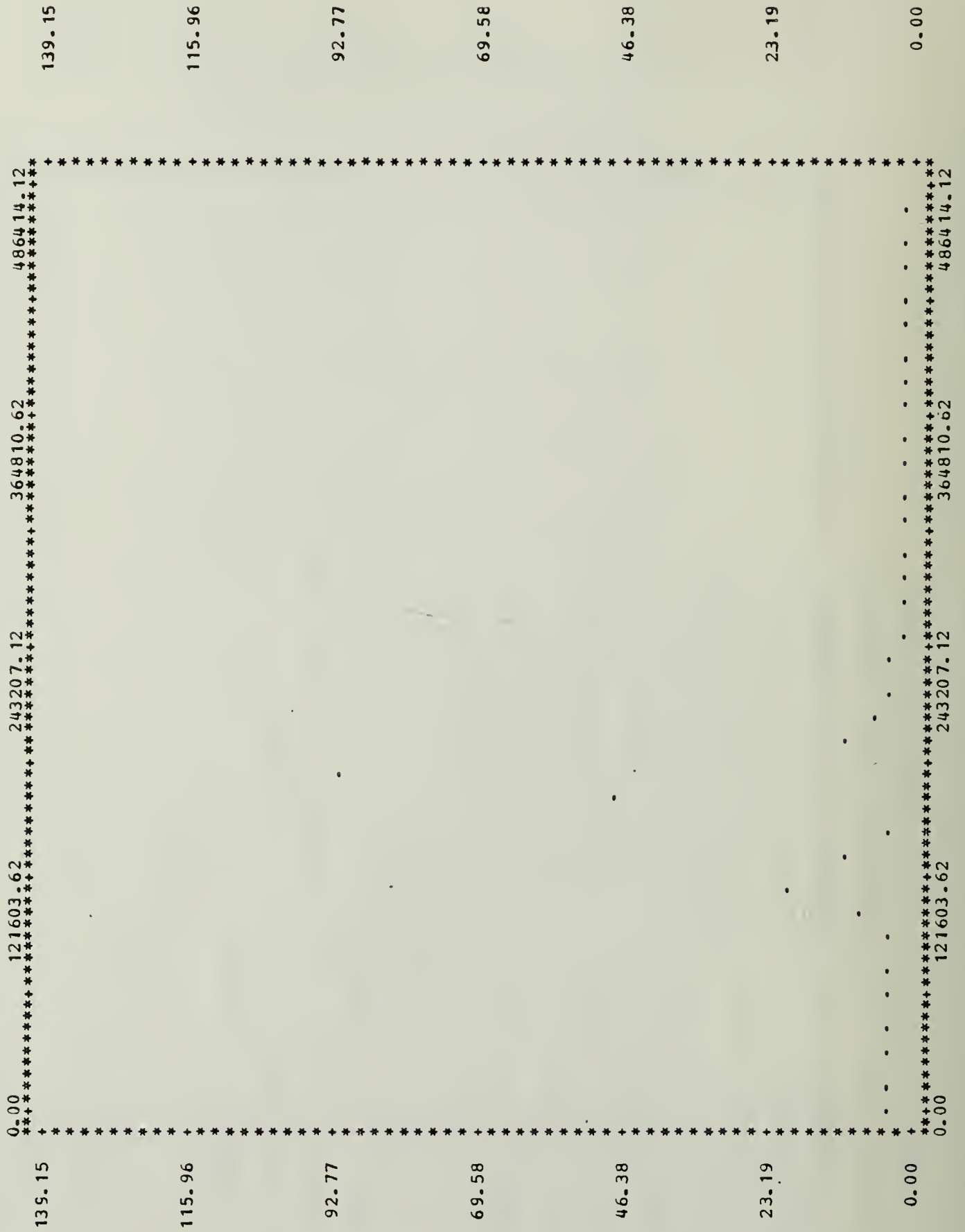
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67.57	0.00				
54.06	0.00				
40.54	0.00				
27.03	0.00				
13.51	0.00				
0.00	0.00	121603.62	243207.12	364810.62	486414.12

N	MEAN	VARIANCE	SKENNESS	KURTOSIS
1	1639783	1709248	113409	106232
2	1694119	1659799	163184	103622
3	2022084	1637973	336020	105181
4	444832	1696003	527175	114977
5	575301	1889410	566105	139688
6	666784	2351081	972265	200388
7	666784	3517560	772265	392306
8	666784	432282	630638	161559
9	666784	519770	401151	770014
10	666784	520733	600273	148756
11	666784	520733	666657	887606
12	666784	520733	666657	887606
13	666784	520733	666657	887606
14	666784	520733	666657	887606
15	666784	520733	666657	887606
16	666784	520733	666657	887606
17	666784	520733	666657	887606
18	666784	520733	666657	887606
19	666784	520733	666657	887606
20	666784	520733	666657	887606
21	666784	520733	666657	887606
22	666784	520733	666657	887606
23	666784	520733	666657	887606
24	666784	520733	666657	887606
25	666784	520733	666657	887606
26	666784	520733	666657	887606
27	666784	520733	666657	887606
28	666784	520733	666657	887606
29	666784	520733	666657	887606
30	666784	520733	666657	887606
31	666784	520733	666657	887606
32	666784	520733	666657	887606
33	666784	520733	666657	887606

N	X	SUM X**2	SUM X**3	X**4	SUM X**4
1	16397831	09841063E+03	13810400	13899991E+04	60282244
2	16941190	10472507E+03	00138939	94587657E+04	22449458
3	18220824	17905823E+03	03393393	10452042E+04	26425104
4	20249444	212605E+03	10843475E+04	98908221E+04	16286988
5	23295753	1573474E+03	333040E+04	15984224E+04	49159842
6	27996184	3339E+03	3845E+04	15984224E+04	90294915
7	35936066	90701501E+03	49133E+04	50720208E+05	13046901
8	52502686	78825291E+03	134313E+04	52383947E+05	48244320
9	14987324	45728772E+04	4934024E+05	15966948E+06	38915966
10	29715319	33822615E+04	5227176E+06	1909063E+08	96331979
11	49319622	5072521E+04	30303E+07	154583E+08	49939545
12	19433195	58019601E+04	4802437E+07	10767533E+09	84839791
13	29556818	66542102E+04	1444010E+07	10767533E+09	1979063E+08
14	11348435	94803092E+03	1500612E+07	22256742E+09	58410767
15	49709048	4803092E+03	1500612E+07	42233144E+09	74469472
16	35327571	10315635E+03	15057830E+05	14749737E+09	74469472
17	28124367	95223995E+03	15057830E+05	36958462E+09	14749737
18	33677526	1199091E+03	1722194E+05	14881906E+09	14749737
19	18526645	63048547E+03	1722194E+05	45150333E+09	10767533
20	16910492	57918267E+03	2422E+04	29742184E+09	45150333
21	15647245	7670945E+03	2422E+04	21187382E+09	21187382
22	14627245	7501172E+03	3678661E+03	16048594E+09	16048594
23	13793611	8878533E+03	3678661E+03	27734396E+09	27734396
24	13102129	7145493E+03	3678661E+03	12773493E+09	12773493
25	12524666	6083759E+03	3678661E+03	90817189E+09	90817189
26	12041969	57391062E+03	151374E+03	80139938E+09	80139938
27	11640703	6484772E+03	1781624E+03	724497179E+09	72449717
28	11311639	5402371E+03	339951E+03	668694310E+09	66869431
29	11049050	4984923E+03	339951E+03	59997200E+09	59997200
30	10850949	517871504E+03	1530E+03	5810861131E+09	58108611
31	10720177	99482293E+03	3530E+03	570282283401E+09	57028228
32	10668961	45745031E+03	166431E+03	566765341940E+09	56676534
33					

MODULATION TECHNIQUE = QPRS
 QPRS CLASS 5 FILTER
 BIPOLAR LOGIC
 BAUD OR SYMBOL RATE = 1200 HZ
 BITS PER BINARY CODE WORD = 2
 BIT RATE = 0.2400000000000000E+04
 CARRIER FREQUENCY = 2400 HZ
 MAXIMUM CARRIER AMPLITUDE = 1 VOLT(S)
 INITIAL PHASE ANGLE = 0 DEGREES
 TIME BETWEEN SAMPLES = 0.6784342273548912E-04 SEC
 NUMBER OF SAMPLES GENERATED = 64
 SEED FOR RANDOM NUMBER GENERATOR = 1
 NUMBER OF TIMES SIMULATION REPEATS = 100
 SUM OF VARIANCES SUM OF VARIANCES**2
 0.2422177865073176E+04 0.1348538369218457E+07
 SUM OF SKEWNESS SUM OF SKEWNESS**2
 -0.8202160755049249E+06 0.2049138949944578E+12
 SUM OF KURTOSIS SUM OF KURTOSIS**2
 0.3582703927263425E+07 0.4782889442290025E+13
 MEAN VARIANCE VARIANCE OF THE VARIANCES
 0.7339932924464169E+02 0.3658600433158962E+05
 MEAN SKEWNESS VARIANCE OF THE SKEWNESS
 -0.2485503259105833E+05 0.5766481178314780E+10
 MEAN KURTOSIS VARIANCE OF THE KURTOSIS
 0.1085667856746492E+06 0.1373102122775966E+12





N	MEAN	VARIANCE	SKENNESS	KURTOSIS
1	317500	979669	977690	3634
2	601994	765044	788736	5813
3	492879	921329	874998	1606
4	050986	669161	290838	3790
5	180736	150713	260191	3282
6	492121	435658	795223	9899
7	646783	203001	390482	1834
8	734938	424764	896485	5035
9	200145	889591	755662	1669
10	540923	215610	755662	4397
11	307109	172333	692445	1753
12	412506	118058	745245	3384
13	540519	849648	919098	6581
14	156644	696486	908802	3599
15	802742	633391	797157	2654
16	577410	880324	959880	1853
17	459631	104764	288448	1976
18	386341	179600	178638	9051
19	336315	582553	474683	1837
20	300326	108183	790580	1497
21	273190	428099	141228	9231
22	252123	441845	605801	2842
23	221985	185742	347386	5282
24	110603	355400	265680	2012
25	202107	551111	274738	2012
26	194757	033912	255480	5733
27	188757	144657	601881	0673
28	183939	664964	841884	1081
29	180200	719831	294681	5072
30	177490	732841	545984	1081
31	175811	235197	718280	8951
32	175226	333447	758108	1809
33				7057

N	X	SUM	X**2	SUM	X**3	SUM	X**4
1	1514	369	1223	785	17E+04	5654	579
2	1553	685	930	1179	85E+04	5895	585
3	1680	656	444	0333	33E+04	6728	605
4	1927	326	833	606	91E+04	8148	757
5	2369	286	953	405	192E+04	1006	805
6	3190	124	392	916	30E+04	1224	935
7	4923	871	368	377	45E+04	1552	1043
8	9847	312	317	680	66E+04	1826	1181
9	5323	771	248	760	04E+05	1900	1290
10	3637	433	625	952	42E+06	2292	1567
11	1176	787	256	917	31E+06	2627	1752
12	2098	376	597	573	33E+06	2755	1895
13	3685	042	312	571	93E+06	2613	1985
14	2933	389	866	334	83E+05	2590	1993
15	7619	838	209	331	78E+04	1392	1590
16	3924	777	969	626	127E+04	2550	1853
17	2494	777	969	626	127E+04	1064	964
18	1774	622	224	584	093E+04	434	477
19	1091	198	917	366	450E+04	369	572
20	1356	637	666	624	462E+04	225	182
21	9118	413	808	433	1990E+03	162	298
22	7850	860	575	300	507E+03	123	227
23	6924	839	470	475	764E+03	91	140
24	6231	593	327	372	087E+03	82	127
25	5297	095	116	754	51E+03	70	100
26	4741	266	931	684	071E+03	62	90
27	4458	173	898	955	488E+03	56	82
28	4424	101	195	361	424E+03	51	76
29	4332	502	267	882	254E+03	46	68
30	4279	130	539	464	648E+03	43	62
31	4261	159	685	782	1065E+03	40	58
32							
33							


```

C      X=0. D0
C      Y=0. D0
C      Z=0. D0
C      DO 30 I=1,15
C          X=X+SUM X(I)
C          Y=Y+SUM XSQ(I)
C          Z=Z+SUM X(I)**2
C      CONTINUE
C      XA=(Z/N) - (X**2/(R*N))
C      XE=Y - (Z/N)
C      TOTAL=Y - (X**2/(R*N))
C      DF1=R-1. D0
C      DF2=R*(N-1. D0)
C      FSTAT=(XA/DF1)/(XE/DF2)
C      *** OUTPUT THE RESULTS-THE FORMATS REPRESENT VARIABLE DEFINITIONS
C      WRITE(6,31) J
C      FORMAT(1,' F-STATISTICS FOR THE',I4,' COMPONENT')
C      WRITE(6,40) X
C      FORMAT(10,' SUM OF SUMS =',E23.16)
C      WRITE(6,41) Y
C      FORMAT(10,' SUM OF SUMS**2 =',E23.16)
C      WRITE(6,42) Z
C      FORMAT(10,' SUM OF SQUARE OF SUMS =',E23.16)
C      WRITE(6,50) XA
C      FORMAT(10,' AMONG GROUP SUM OF SQUARES =',E23.16)
C      WRITE(6,51) XE
C      FORMAT(10,' WITHIN GROUP SUM OF SQUARES =',E23.16)
C      WRITE(6,60) TOTAL
C      FORMAT(10,' TOTAL SUM OF SQUARES =',E23.16)
C      WRITE(6,70) DF1
C      FORMAT(10,' DEGREES OF FREEDOM IN NUMERATOR =',E23.16)
C      WRITE(6,71) DF2
C      FORMAT(10,' DEGREES OF FREEDOM IN DENOMINATOR =',E23.16)
FTE 00450
FTE 00460
FTE 00470
FTE 00480
FTE 00490
FTE 00500
FTE 00510
FTE 00520
FTE 00530
FTE 00540
FTE 00550
FTE 00560
FTE 00570
FTE 00580
FTE 00590
FTE 00600
FTE 00610
FTE 00620
FTE 00630
FTE 00640
FTE 00650
FTE 00660
FTE 00670
FTE 00680
FTE 00690
FTE 00700
FTE 00710
FTE 00720
FTE 00730
FTE 00740
FTE 00750
FTE 00760
FTE 00770
FTE 00780
FTE 00790
FTE 00800
FTE 00810
FTE 00820
FTE 00830
FTE 00840
FTE 00850
FTE 00860
FTE 00870
FTE 00880
FTE 00890
FTE 00900
FTE 00910
FTE 00920
FTE 00930
FTE 00940

```

```
80 WRITE(6,80) FSTAT  
C  FORMAT('0.', 'F-STATISTIC =', E23.16)  
100 CONTINUE  
C  
81 WRITE(6,81)  
C  FORMAT('1.}')  
STOP  
END
```

```
FTE00950  
FTE00960  
FTE00970  
FTE00980  
FTE00990  
FTE01000  
FTE01010  
FTE01020  
FTE01030
```

APPENDIX E
RESULTS OF F-TEST

F-STATISTICS FOR THE 1 COMPONENT

SUM OF SUMS = 0.2091487882294994D 02
SUM OF SUMS**2 = 0.1810655469453404D 02
SUM OF SQUARE OF SUMS = 0.4128097510679048D 02
AMCNG GROUP SUM OF SQUARES = 0.1211883136154515D 00
WITHIN GROUP SUM OF SQUARES = 0.1769374494346614D 02
TOTAL SUM OF SQUARES = 0.1781493325708159D 02
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.7265063214387600D 00

F-STATISTICS FOR THE 2 COMPONENT

SUM OF SUMS = 0.2305792717805020D 02
SUM OF SUMS**2 = 0.1894701234015291D 02
SUM OF SQUARE OF SUMS = 0.4663825126655468D 02
AMCNG GROUP SUM OF SQUARES = 0.1119371755000360D 00
WITHIN GROUP SUM OF SQUARES = 0.1848062982748736D 02
TOTAL SUM OF SQUARES = 0.1859256700298739D 02
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.6424746465014737D 00

F-STATISTICS FOR THE 3 COMPONENT

SUM OF SUMS = 0.2693734535827635D 02
SUM OF SUMS**2 = 0.2124674921974186D 02
SUM OF SQUARE OF SUMS = 0.5921566381358867D 02
AMCNG GROUP SUM OF SQUARES = 0.1084095881685183D 00
WITHIN GROUP SUM OF SQUARES = 0.2065459258160598D 02
TOTAL SUM OF SQUARES = 0.2076300216977449D 02
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.5567362242775778D 00

F-STATISTICS FOR THE 4 COMPONENT

SUM OF SUMS = 0.3175688631627065D 02
SUM OF SUMS**2 = 0.2621104542300214D 02
SUM OF SQUARE OF SUMS = 0.8070513093726266D 02
AMONG GROUP SUM OF SQUARES = 0.1347180903696015D 00
WITHIN GROUP SUM OF SQUARES = 0.2540399411362951D 02
TOTAL SUM OF SQUARES = 0.2553871220399911D 02
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04

F-STATISTIC = 0.5624997485041869D 00

F-STATISTICS FOR THE 5 COMPONENT

SUM OF SUMS = 0.3669104349531116D 02
SUM OF SUMS**2 = 0.3380633740317695D 02
SUM OF SQUARE OF SUMS = 0.1069682473356158D 03
AMONG GROUP SUM OF SQUARES = 0.1721940248396148D 00
WITHIN GROUP SUM OF SQUARES = 0.3273665492982079D 02
TOTAL SUM OF SQUARES = 0.3290884895466041D 02
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04

F-STATISTIC = 0.5579331866788867D 00

F-STATISTICS FOR THE 6 COMPONENT

SUM OF SUMS = 0.4160097878948431D 02
SUM OF SUMS**2 = 0.4313236642020094D 02
SUM OF SQUARE OF SUMS = 0.1408215358007360D 03
AMONG GROUP SUM OF SQUARES = 0.2544544005119440D 00
WITHIN GROUP SUM OF SQUARES = 0.4172415106219358D 02
TOTAL SUM OF SQUARES = 0.4197860546270552D 02
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04

F-STATISTIC = 0.6468757561623442D 00

F-STATISTICS FOR THE 7 COMPONENT

SUM OF SUMS = 0.4810387092348111D 02
SUM OF SUMS**2 = 0.5206409381611744D 02
SUM OF SQUARE OF SUMS = 0.1964653659903027D 03
AMONG GROUP SUM OF SQUARES = 0.4219987280210724D 00
WITHIN GROUP SUM OF SQUARES = 0.5009944015621441D 02
TOTAL SUM OF SQUARES = 0.5052143888423548D 02
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.8934632362547178D 00

F-STATISTICS FOR THE 8 COMPONENT

SUM OF SUMS = 0.5623255941290002D 02
SUM OF SUMS**2 = 0.8590285622098203D 02
SUM OF SQUARE OF SUMS = 0.3070018365343552D 03
AMONG GROUP SUM OF SQUARES = 0.9619512065933320D 00
WITHIN GROUP SUM OF SQUARES = 0.8283283785563848D 02
TOTAL SUM OF SQUARES = 0.8379478906223181D 02
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.1231824736914027D 01

F-STATISTICS FOR THE 9 COMPONENT

SUM OF SUMS = 0.9931605295569187D 02
SUM OF SUMS**2 = 0.4043531056175881D 03
SUM OF SQUARE OF SUMS = 0.1416642417283150D 04
AMONG GROUP SUM OF SQUARES = 0.7590638589699638D 01
WITHIN GROUP SUM OF SQUARES = 0.3901866814447566D 03
TOTAL SUM OF SQUARES = 0.3977773200344562D 03
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.2063499133280512D 01

F-STATISTICS FOR THE 10 COMPONENT

SUM OF SUMS = 0.2029942628781924D 03
SUM OF SUMS**2 = 0.1757564757819924D 04
SUM OF SQUARE OF SUMS = 0.7655692250451960D 04
AMCNG GROUP SUM OF SQUARES = 0.4908580866354581D 02
WITHIN GROUP SUM OF SQUARES = 0.1681007835315404D 04
TOTAL SUM OF SQUARES = 0.1730093643978950D 04
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.3097309684192641D 01

F-STATISTICS FOR THE 11 COMPONENT

SUM OF SUMS = 0.2004773302247246D 03
SUM CF SUMS**2 = 0.1811875077561617D 04
SUM OF SQUARE OF SUMS = 0.7980439863108266D 04
AMCNG GROUP SUM OF SQUARES = 0.5301029200839379D 02
WITHIN GROUP SUM OF SQUARES = 0.1732070678930534D 04
TOTAL SUM OF SQUARES = 0.1785080970938928D 04
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.3246332537532912D 01

F-STATISTICS FOR THE 12 COMPONENT

SUM OF SUMS = 0.2210834652773109D 03
SUM CF SUMS**2 = 0.2165859765218944D 04
SUM OF SQUARE OF SUMS = 0.9414279932820438D 04
AMCNG GROUP SUM OF SQUARES = 0.6155753358218842D 02
WITHIN GROUP SUM OF SQUARES = 0.2071716965890740D 04
TOTAL SUM OF SQUARES = 0.2133274499472928D 04
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.3151731454585565D 01

F-STATISTICS FOR THE 13 COMPONENT

SUM OF SUMS = 0.1979583434471791D 03
SUM OF SUMS**2 = 0.1904701075347160D 04
SUM OF SQUARE OF SUMS = 0.7185446672840862D 04
AMCNG GROUP SUM OF SQUARES = 0.4572946290150773D 02
WITHIN GROUP SUM OF SQUARES = 0.1832846608618751D 04
TOTAL SUM OF SQUARES = 0.1878576071520259D 04
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.2646478671459864D 01

F-STATISTICS FOR THE 14 COMPONENT

SUM OF SUMS = 0.9227736272614619D 02
SUM OF SUMS**2 = 0.2600827196886254D 03
SUM OF SQUARE OF SUMS = 0.9540726819081072D 03
AMCNG GROUP SUM OF SQUARES = 0.3863985704619236D 01
WITHIN GROUP SUM OF SQUARES = 0.2505419928695444D 03
TOTAL SUM OF SQUARES = 0.2544059785741636D 03
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.1635887377498235D 01

F-STATISTICS FOR THE 15 COMPONENT

SUM OF SUMS = 0.6880926336210145D 02
SUM OF SUMS**2 = 0.1018300362534556D 03
SUM OF SQUARE OF SUMS = 0.3695062863415098D 03
AMCNG GROUP SUM OF SQUARES = 0.5385863804584070D 00
WITHIN GROUP SUM OF SQUARES = 0.9813497339004056D 02
TOTAL SUM OF SQUARES = 0.9867355977049896D 02
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.5821433971075596D 00

F-STATISTICS FOR THE 16 COMPONENT

SUM OF SUMS = 0.6961387326450431D 02
SUM OF SUMS**2 = 0.1137157033969463D 03
SUM OF SQUARE OF SUMS = 0.3597053597878584D 03
AMCNG GROUP SUM OF SQUARES = 0.3663260306209388D 00
WITHIN GROUP SUM OF SQUARES = 0.1101186497990677D 03
TOTAL SUM OF SQUARES = 0.1104849758296886D 03
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.3528623485827816D 00

F-STATISTICS FOR THE 17 COMPONENT

SUM OF SUMS = 0.7052854165691613D 02
SUM OF SUMS**2 = 0.1548042004914454D 03
SUM OF SQUARE OF SUMS = 0.3820324148469269D 03
AMCNG GROUP SUM OF SQUARES = 0.5041406896350342D 00
WITHIN GROUP SUM OF SQUARES = 0.1509838763429761D 03
TOTAL SUM OF SQUARES = 0.1514880170326111D 03
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.3541763825767676D 00

F-STATISTICS FOR THE 18 COMPONENT

SUM OF SUMS = 0.7950452893326030D 02
SUM OF SUMS**2 = 0.1454127656122291D 03
SUM OF SQUARE OF SUMS = 0.5157161626920556D 03
AMCNG GROUP SUM OF SQUARES = 0.9431815463208067D 00
WITHIN GROUP SUM OF SQUARES = 0.1402556039853086D 03
TOTAL SUM OF SQUARES = 0.1411987855316294D 03
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.7133020797581566D 00

F-STATISTICS FOR THE 19 COMPONENT

SUM OF SUMS = 0.8206200282896035D 02
SUM OF SUMS**2 = 0.1642503769158388D 03
SUM OF SQUARE OF SUMS = 0.5788746875066006D 03
AMCNG GROUP SUM OF SQUARES = 0.1299298669532475D 01
WITHIN GROUP SUM OF SQUARES = 0.1584616300407728D 03
TOTAL SUM OF SQUARES = 0.1597609287103052D 03
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.8697276809711277D 00

F-STATISTICS FOR THE 20 COMPONENT

SUM OF SUMS = 0.9520048302882186D 02
SUM OF SUMS**2 = 0.2094086558414699D 03
SUM OF SQUARE OF SUMS = 0.8713219218815827D 03
AMCNG GROUP SUM OF SQUARES = 0.2671131239535162D 01
WITHIN GROUP SUM OF SQUARES = 0.2006954366226541D 03
TOTAL SUM OF SQUARES = 0.2033665678621893D 03
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.1411744637781583D 01

F-STATISTICS FOR THE 21 COMPONENT

SUM OF SUMS = 0.8994139952150146D 02
SUM OF SUMS**2 = 0.2335862791765991D 03
SUM OF SQUARE OF SUMS = 0.7245755635510632D 03
AMCNG GROUP SUM OF SQUARES = 0.1852785403586404D 01
WITHIN GROUP SUM OF SQUARES = 0.2263405235410884D 03
TOTAL SUM OF SQUARES = 0.2281933089446748D 03
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.8682828488687504D 00

F-STATISTICS FOR THE 22 COMPONENT

SUM OF SUMS = 0.1035648300735959D 03
SUM OF SUMS**2 = 0.2414810868436007D 03
SUM OF SQUARE OF SUMS = 0.9427341493765320D 03
AMCNG GROUP SUM OF SQUARES = 0.2276892141650119D 01
WITHIN GROUP SUM OF SQUARES = 0.2320537453498354D 03
TOTAL SUM OF SQUARES = 0.2343306374914855D 03
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.1040764077320930D 01

F-STATISTICS FOR THE 23 COMPONENT

SUM OF SUMS = 0.9031234717154746D 02
SUM OF SUMS**2 = 0.2047768116906234D 03
SUM OF SQUARE OF SUMS = 0.7149379755971323D 03
AMCNG GROUP SUM OF SQUARES = 0.1711833054881912D 01
WITHIN GROUP SUM OF SQUARES = 0.1976274319346521D 03
TOTAL SUM OF SQUARES = 0.1993392649895340D 03
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.9187822552243536D 00

F-STATISTICS FOR THE 24 COMPONENT

SUM OF SUMS = 0.9171706807335522D 02
SUM OF SUMS**2 = 0.1900438745495707D 03
SUM OF SQUARE OF SUMS = 0.8139562480340389D 03
AMCNG GROUP SUM OF SQUARES = 0.2531548763025405D 01
WITHIN GROUP SUM OF SQUARES = 0.1819043120692303D 03
TOTAL SUM OF SQUARES = 0.1844358608322557D 03
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.1476188171339999D 01

F-STATISTICS FOR THE 25 COMPONENT

SUM OF SUMS = 0.8440126623444366D 02
SUM OF SUMS**2 = 0.1782254895437147D 03
SUM OF SQUARE OF SUMS = 0.6892901073945840D 03
AMCNG GROUP SUM OF SQUARES = 0.2143851912627546D 01
WITHIN GROUP SUM OF SQUARES = 0.1713325884697689D 03
TOTAL SUM OF SQUARES = 0.1734764403823964D 03
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.1327251499840134D 01

F-STATISTICS FOR THE 26 COMPONENT

SUM OF SUMS = 0.6923579472492147D 02
SUM OF SUMS**2 = 0.1481985058366125D 03
SUM OF SQUARE OF SUMS = 0.4452980334185913D 03
AMCNG GROUP SUM OF SQUARES = 0.1257250153391605D 01
WITHIN GROUP SUM OF SQUARES = 0.1437455255024266D 03
TOTAL SUM OF SQUARES = 0.1450027756558182D 03
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.9277389287476910D 00

F-STATISTICS FOR THE 27 COMPONENT

SUM OF SUMS = 0.6366092822129744D 02
SUM OF SUMS**2 = 0.1177906819912730D 03
SUM OF SQUARE OF SUMS = 0.3935159041535181D 03
AMCNG GROUP SUM OF SQUARES = 0.1233349853537058D 01
WITHIN GROUP SUM OF SQUARES = 0.1138555229497378D 03
TOTAL SUM OF SQUARES = 0.1150888728032749D 03
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.1149027974258136D 01

F-STATISTICS FOR THE 28 COMPONENT

SUM OF SUMS = 0.5387592494868525D 02
SUM OF SUMS**2 = 0.1186133442790129D 03
SUM OF SQUARE OF SUMS = 0.2792595957915495D 03
AMCNG GROUP SUM OF SQUARES = 0.8575190985312517D 00
WITHIN GROUP SUM OF SQUARES = 0.1158207483210974D 03
TOTAL SUM OF SQUARES = 0.1166782674196286D 03
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.7853366268738306D 00

F-STATISTICS FOR THE 29 COMPONENT

SUM OF SUMS = 0.4536144151906700D 02
SUM OF SUMS**2 = 0.6564305139058856D 02
SUM OF SQUARE OF SUMS = 0.1919053830677748D 03
AMONG GROUP SUM OF SQUARES = 0.5472802462192574D 00
WITHIN GROUP SUM OF SQUARES = 0.6372399755991081D 02
TOTAL SUM OF SQUARES = 0.6427127780613007D 02
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.9109723144851782D 00

F-STATISTICS FOR THE 30 COMPONENT

SUM OF SUMS = 0.3732568029970994D 02
SUM OF SUMS**2 = 0.5705765228634419D 02
SUM OF SQUARE OF SUMS = 0.1284820507967475D 03
AMCNG GROUP SUM OF SQUARES = 0.3560162347433721D 00
WITHIN GROUP SUM OF SQUARES = 0.5577283177837672D 02
TOTAL SUM OF SQUARES = 0.5612884801312009D 02
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.6770886363437515D 00

F-STATISTICS FOR THE 31 COMPONENT

SUM OF SUMS = 0.2973876286269883D 02
SUM OF SUMS**2 = 0.4217833610659068D 02
SUM OF SQUARE OF SUMS = 0.7726205204918280D 02
AMONG GROUP SUM OF SQUARES = 0.1830245094226048D 00
WITHIN GROUP SUM OF SQUARES = 0.4140571558609885D 02
TOTAL SUM OF SQUARES = 0.4158874009552145D 02
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.4688645251806333D 00

F-STATISTICS FOR THE 32 COMPONENT

SUM OF SUMS = 0.2142367689889270D 02
SUM OF SUMS**2 = 0.1414820425416038D 02
SUM OF SQUARE OF SUMS = 0.3565723402182890D 02
AMONG GROUP SUM OF SQUARES = 0.5058971897285643D-01
WITHIN GROUP SUM OF SQUARES = 0.1379163191394209D 02
TOTAL SUM OF SQUARES = 0.1384222163291495D 02
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.3890854828465455D 00

F-STATISTICS FOR THE 33 COMPONENT

SUM OF SUMS = 0.1732004830070321D 02
SUM OF SUMS**2 = 0.1115582097066481D 02
SUM OF SQUARE OF SUMS = 0.2312899538600082D 02
AMONG GROUP SUM OF SQUARES = 0.3130057176754676D-01
WITHIN GROUP SUM OF SQUARES = 0.1092453101680480D 02
TOTAL SUM OF SQUARES = 0.1095583158857235D 02
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.1485000000000000D 04
F-STATISTIC = 0.3039120267386334D 00

F-STATISTICS OF MEAN VARIANCE, SKEWNESS AND KURTOSIS

F-STATISTICS FOR THE 1 COMPONENT

SUM OF SUMS = 0.1111617439422250D 05
SUM OF SUMS**2 = 0.4319425777749392D 07
SUM OF SQUARE OF SUMS = 0.1861260733960752D 08
AMONG GROUP SUM OF SQUARES = 0.3143833877400904D 06
WITHIN GROUP SUM OF SQUARES = 0.3755407373518861D 07
TOTAL SUM OF SQUARES = 0.4069790761258952D 07
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.4800000000000000D 03
F-STATISTIC = 0.2870223636519026D 01

F-STATISTICS FOR THE 2 COMPONENT

SUM OF SUMS = -0.3062348822555926D 07
SUM OF SUMS**2 = 0.7751235739069674D 12
SUM OF SQUARE OF SUMS = 0.2376364181020636D 13
AMONG GROUP SUM OF SQUARES = 0.5306562101878761D 11
WITHIN GROUP SUM OF SQUARES = 0.7031125381184634D 12
TOTAL SUM OF SQUARES = 0.7561781591372509D 12
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.4800000000000000D 03
F-STATISTIC = 0.2587626620217669D 01

F-STATISTICS FOR THE 3 COMPONENT

SUM OF SUMS = 0.1087692759375071D 08
SUM OF SUMS**2 = 0.1368235571001090D 14
SUM OF SQUARE OF SUMS = 0.3521258942662316D 14
AMONG GROUP SUM OF SQUARES = 0.8280430048704694D 12
WITHIN GROUP SUM OF SQUARES = 0.1261530754556778D 14
TOTAL SUM OF SQUARES = 0.1344335055043825D 14
DEGREES OF FREEDOM IN NUMERATOR = 0.1400000000000000D 02
DEGREES OF FREEDOM IN DENOMINATOR = 0.4800000000000000D 03
F-STATISTIC = 0.2250444214596077D 01

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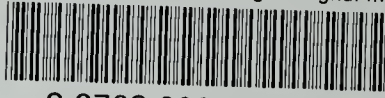
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